Personal Computer
Circuit Design
Tools



IsSpice4 User's Guide

Volumes 1 and 2

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About IsSpice4

Berkeley SPICE 3A.7 was released in 1984. It was one of the first attempts by the University of California at Berkeley to enhance the standard version of SPICE used around the world, SPICE 2G.6. Since that time, “version 3” has gone through a number of major revisions. However, it was not until version 3E.2, which was released in early 1992, that there was a viable replacement for SPICE 2G.6. This is due to the fact that 3E.2 was the first version of Berkeley SPICE 3 to contain virtually all of the capabilities of SPICE 2G.6. IsSpice3 was the first SPICE program to be based on SPICE 3E.2 when it was released in 1992. Some SPICE vendors have chosen to upgrade their SPICE 2G.6 versions by adding pieces of SPICE 3. Intusoft has chosen to provide a simple and powerful one-step upgrade to the new standard in simulation.

With IsSpice4, Intusoft has added a breadth of powerful interactive features to SPICE 3F5, maintaining IsSpice4’s leadership of truly interactive performance. It also includes a number of extensions in XSPICE, a derivative of Berkeley SPICE originally produced at the Georgia Institute of Technology.

In addition to porting SPICE 3 to the PC, Intusoft has added enhancements above and beyond the Berkeley version. The following pages detail some of the differences between Intusoft’s implementation, IsSpice4, which is currently based on Berkeley SPICE 3F.5, and previous versions of SPICE.

SPICE 2/IsSpice4 Differences

IsSpice4 is a derivative of Berkeley SPICE 3F.5. There are a number of major differences between IsSpice4, past IsSpice versions, and competitive versions of SPICE. Please take a moment to read through the following sections about the program differences, especially the “Error Checking” section.

User Interface

The Windows version of IsSpice4 is a (WIN32s) 32-bit program, and supportsWindows 98SE/ME, and NT4/2000/XP/Vista.

IsSpice4 is completely interactive. Simulations can be started, stopped, paused and resumed on demand. New analyses can be run at any time. Virtually any component or model parameter can be hand tweaked, individually or in groups, and the circuit can be instantly resimulated. Voltage, current, and power dissipation waveforms may be displayed at any time.

IsSpice4 contains direct links to "SpiceNet" design entry and IntuScope waveform processing systems, allowing simulation data to be available to the schematic for interactive cross-probing, or to the post-processor for instant display even during an analysis.

IsSpice4 displays multiple waveforms from the AC, DC, Transient, Distortion, and Noise analyses, while the simulation runs. This is in contrast to other SPICE versions that display only the timestep and the data for one node voltage or branch current. The number of waveforms that can be displayed is selectable by the user.

IsSpice4 contains a powerful set of interactive command language (ICL) commands that it uses to automatically access things like Print expressions, device parameter variation, simulation breakpoints and control, plus special waveform processing functions. Optionally, the user can write their own “Simulation Scripts," or modify existing ones, to perform special interaction with the simulator and waveform viewer.

Netlist Construction automatically contains these features:

Several display functions located on the Options Menu of SpiceNet, and its toolbar of icons, allow the quick toggle on/off capability for things like pin numbers, part labels, node numbers and labels, operating point values, waveforms and custom artwork.

The "Find" function, located on the Edit Menu of SpiceNet, allows you to find and highlight any part and/or node in your drawing.

A Yes/No option is contained in the Test Point Part Properties Dialog to automatically generate .PRINT statements for distortion analysis.

The Place Subdrawing dialog sorts folders and directories alphanumerically.

SpiceNet allows the simulation of read-only drawing (.DWG) files.

The MakeDB utility automatically opens a log file if an error has occured during the parts database compilation process.

The Update Cache function recognizes all model library file changes, including mechanical properties information.

Cross-probing from schematic to waveform viewer is automated.

Model names and reference designations can use any number of characters. IsSpice4 input netlists may be in upper or lower case, or a mixture of both. Note: entries such as R1 and r1 are equivalent.

IsSpice4 accepts names in place of node numbers from a netlist.

Negative capacitor and inductor values may be used.

Commas are not always used as delimiters. When a comma appears within a set of parentheses, it will be interpreted as a comma. Commas that are not enclosed in parentheses will be treated as spaces.

IsSpice4 automatically converts SPICE 2 dependent source (E, F, G, H) polynomial syntax to the (B) nonlinear dependent source syntax, allowing backward compatibility with any model library using dependent sources.

Support is provided for parameter passing including .PARAM statements, multiple level passing, and expressions in the main circuit.

Error Checking

Errors are placed in the Errors and Status window, and in a file with the same name as the input netlist and the extension .ERR. For example, if the input is Sample.Cir, the error file will be Sample.Err. Some errors may also be repeated in the IsSpice4 output file. If the simulation aborts or the data looks drastically incorrect, you should check the filename.ERR file for a summary listing of errors. This is in contrast to SPICE 2, which places the errors in the output file.

New EKV Model

Addition of the EPLF-EKV 2.6 MOSFET model , a scalable and compact MOSFET model ideal for use in the design and simulation of low-voltage, low-current analog, and mixed analog-digital circuits using submicron CMOS technologies.

Latest BSIM 4 Model

This model addresses many issues in modeling sub-0.13 micron CMOS technology and RF high-speed CMOS circuit simulation. BSIM4.0.0 has the following major improvements and additions over BSIM3v3:

- An accurate new model of the intrinsic input resistance for both RF, high-frequency analog and high-speed digital application.
- Flexible substrate resistance network for RF modeling.
- A new accurate channel thermal noise model and a noise partition model for the induced gate noise.
- A non-quasi-static (NQS) model that is consistent with the Rg-based RF model and a consistent AC model that ac counts for the NQS effect in both transconductances and capacitances.

- An accurate gate direct tunneling model.
- A comprehensive and versatile geometry-dependent parasitics model for various source/drain connections and multi-finger devices.
- Improved model for steep vertical retrograde doping profiles.
- Better model for pocket-implanted devices in Vth, bulk charge effect model, and Rout.

Powerful Models Written in C

Code models are a unique type of SPICE model, created using a publicly available AHDL (Analog Hardware Description Language) based on the C programming language. The code describing the model's behavior is linked to the simulator via an external DLL file rather than being bound within the executable program. This allows new primitive models to be added to the simulator, and old models changed, without having to recompile IsSpice4. You can add your own code models to IsSpice4 using the Intusoft Code Modeling Kit. The modeling kit produces a DLL that can be read by any IsSpice4 program. Dozens of analog, digital, and mixed analog/digital code models are included in IsSpice4.

Unique and Improved SPICE Elements

A variety of new analog behavioral capabilities are included in IsSpice4. The nonlinear dependent source element (B) allows you to access in-line equations using algebraic, trigonometric or transcendental operators, node voltages and currents. If-Then-Else functions and Boolean logic expressions, useful for mixed-mode simulation, can also be entered directly.

A variety of new models are included in the IsSpice4 program:

- Lossy transmission line model using a distributed approach (RC, RG, LC, and RLC combinations)
- Uniformly distributed RC/RD transmission line model
- Additional GaAs Mesfet models based on Statz, Curtis-Ettenburg and others
- Mosfet models (BSIM4.3.0, 3v3.2, Level 6-8, FD SOI)

- Smooth transition switch
- Voltage and current-controlled switches with hysteresis
- Semiconductor resistor and capacitor .MODEL statements
- Improved MOSFET level 2 model (capacitance response)
- New JFET model (several new parameters)
- Improved lossless transmission line model (Dynamic breakpoint table with minimum breakpoint spacing control)

New and Improved Analysis Capabilities*

IsSpice4 includes a 12-state digital logic simulator, which provides Native Mixed-Mode simulation capability. Event-driven simulation algorithms are also provided for real data, which allows sampled data filters to be simulated.

A VSECTOL option has been added for accurate simulation of fast pulses. DCCONV and TRANCONV options have been added to help hard to converge circuits in dc and transient analysis.

An ICSTEP option has been added for high-gain feedback design, and for the modeling and simulation of complex ICs

The ACCT flag, used to produce a summary listing of accounting and simulation related information, now also results in a listing of parts statistics for the circuit.

You can request that IsSpice4 stop a simulation when a voltage, current, or a computed device parameter meets a particular condition. Simulation Breakpoints can be used to test for a variety of conditions including device breakdown, safe operating area, and time-dependent events, all while the simulation is running.

Tolerances are allowed in parameter passing.

Pole-Zero transfer function analysis is supported by IsSpice4.

RSS, EVA, Worst Case and Sensitivity (Sensitivity in time, AC and DC domains) analyses are available.

The individual operating temperature of a single device can be set to a different value than the overall circuit temperature. This allows simulation of a "hot" component. Temperature and component parametric sweeps can be run for virtually any parameter.

The DC and transient convergence properties of IsSpice4 have been greatly improved through the addition or enhancement of:

- Gmin stepping/Source Stepping algorithms
- Independent Supply Ramping algorithms*
- Improved program defaults, LIMPTS/ITL5 no longer needed
- Alternate UIC algorithm
- Automatic conductance from every node to ground

Enhanced Program Output Features

• Real-time viewing and printing of a wide variety of computed device parameters, such as device power dissipation, inductor flux, BJT Vbe, and FET transconductance. (For BOTH the operating point AND the Transient analysis, see Appendix B in the on-line help for a full summary listing)

• Access to ALL node voltages, power dissipation of any component, and the current through any component, without the need for extra voltage sources.

• Expressions using voltages, currents, computed device parameters and a variety of mathematical functions viewed on-screen immediately after an IsSpice4 run, or saved to the output file for viewing in IntuScope.

• Computed device parameters, voltages, currents and expressions available for devices that are within subcircuits.

• Powerful “Show” and “Showmod” functions with summary printouts of device and model operating point information.

Additions over Berkeley SPICE 3F.5

In addition to the enhancements over the Berkeley SPICE 2G.6 version, Intusoft has added a number of major features to IsSpice4 that are not found in Berkeley SPICE 3F.5.

A graphical interface that allows the user to easily interact with the simulator, including pop-up help menus to support all of the SPICE 3, Nutmeg, and ICL commands.

IsSpice4 features “Real-Time View Windows” that display voltage, current and computed device parameters from the AC, DC, Transient, Distortion, and Noise analyses, and as the simulation runs. A new control statement, “.VIEW,” has been added to provide control of the waveform scaling.

XSPICE enhancements include: Full native mixed-mode simulation, support for user-defined C-subroutines (Code Models), AHDL language based on C, and over 40 new code-model primitives.

The Nutmeg and SPICE3 interactive control commands (Alias, Alter, Let, Save, Set, Show, Showmod, Stop, and Control Loop) are vastly augmented.

The SPICE 3 B element (arbitrary dependent source) supports Boolean logic expressions, and an If-Then-Else statement. This is useful for a variety of functions, including table-type representations.

A new JFET and HEMT model (Parker model) based on the work of Macquarie University in Australia has been added.

A model current convergence test has been added to IsSpice4.

The Lossy Transmission Line has frequency dependence (skin effect/dielectric loss) in the time and frequency domains.

R, L, C, B, and O expressions can use frequency, time and temperature.

B elements accept expressions that are functions of device currents in the time and frequency domains.

Element Syntax Changes

Temperature coefficients are no longer included on the resistor call line. Resistor temperature coefficients are now inserted in a resistor .MODEL statement.

The MOSFET parameter XQC is ignored since an improved Meyer capacitance model is used all of the time.

Control Statement Syntax Changes

The .NOISE and .DISTO statements have new syntax requirements. SPICE 2 .NOISE and .DISTO syntax is not compatible. See the .NOISE and .DISTO syntax in Chapter 10 for more information.

The .TEMP statement is not recognized. To change the circuit temperature, use the .OPTIONS TEMP= parameter or the *set temp* = ICL command. Multiple runs at several temperatures are fully supported. In addition, a different temperature can be set on each individual device during a single simulation.

Several .OPTIONS parameters have been added to support the “Real-Time View Windows” and the Boolean logic expressions in the analog behavioral element B. See the .OPTIONS statement for more information.

Several .OPTIONS parameters have been added to support the native mixed-mode simulation features.

Obsolete SPICE 2 Functions
Polynomial capacitors/inductors (using the POLY keyword) are not supported, although polynomial elements can be created using behavioral expressions, subcircuits, the new B element or code models.

Several unnecessary .OPTIONS parameters (ITL5, LIMPTS, etc.) have also been removed.

Several separate input circuit netlists may not be included in the same input file and simulated batch style.

Using IsSpice4

IsSpice4 Overview

IsSpice4 is a significantly enhanced version of SPICE, unlike any analog/ mixed-signal simulator you have run before. This chapter will describe the operation of IsSpice4 and its features. A tutorial on IsSpice4 can be found in the Getting Started manual.

Starting IsSpice4

To run IsSpice4

- Select the Simulate function from the ACTIONS menu in the schematic, text editor, or IntuScope windows.

If IsSpice4 is running, the ACTIONS Simulate function will simply transfer you to IsSpice4.

If you are running a simulation using only a netlist, then select 'Use Text Netlist' from the ICAP_4 Start menu. A dialog will come up asking the directory of your .CIR file. Once selected, you can launch a simulation by clicking the Launch Spice icon in the ICAPS Program Selector dialog. It will always close the current IsSpice4 simulation and rerun a simulation from the beginning.

Initially, IsSpice4 will load the SPICE netlist and run the simulations that are designated in the netlist, just like previous versions of IsSpice. Once the initial simulation is complete, the Simulation Control dialog will be displayed, and you will be able to interact with the simulation.

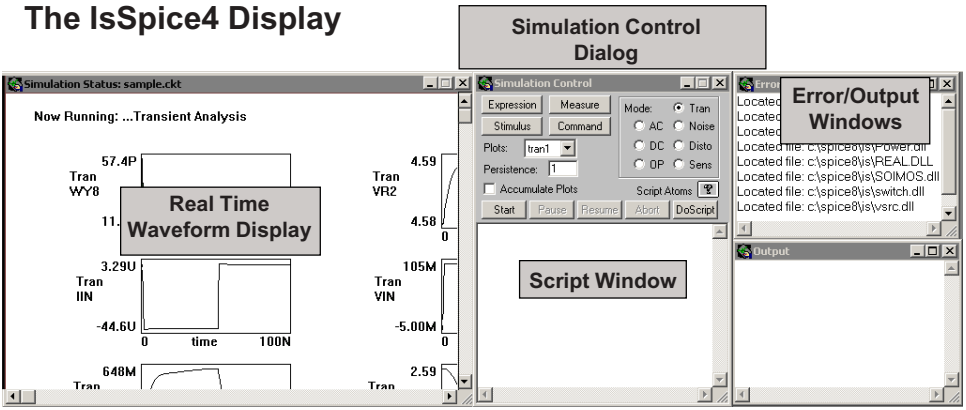
Quitting IsSpice4

To Quit IsSpice4

- Select Quit from the FILE menu.

Quitting IsSpice4 will result in the creation of a standard SPICE output file.

The IsSpice4 Display



The IsSpice4 display presents several different windows: a **Real-Time display**, a **Simulation Control dialog**, and **Error** and **Output** Windows. The Simulation Control window has several buttons that can activate other windows. They are described later in this chapter.

The Real-Time display shows the circuit performance as the simulation runs. At the top of the display is a status line that begins with a status character that alternates between a + and a - sign. This "pulse" let's you know that the simulation is proceeding normally.

ICAP/4Rx does not support some of the interactive IsSpice4 features. The Simulation Control dialog will appear different in ICAP/4Rx.

Waveform Display
The order of waveform display is AC, DC, Transient, Distortion, and then Noise. If more than one analysis is run, data from the AC analysis will be displayed first, then the DC, and so on. IsSpice4 will try to display all of the waveforms listed in the .PRINT and .VIEW and ICL view statements. Print Expressions made with the ICL alias function will be displayed after each analysis is complete. The screen will be filled with waveforms as the simulation progresses, until no more room is available. IsSpice4 will run all of the analyses requested in the netlist, even if the screen is filled with waveforms. Any waveforms not displayed can still be viewed by scrolling the display window.

On the PC, the initial number of waveforms displayed depends on the graphics resolution. The higher the resolution, the more waveforms you can display.

Note: Waveforms will not appear unless an AC, DC, Transient, Distortion, or Noise analysis is run. Also, if the .TRAN TSTART parameter (delayed data taking time) is specified, waveforms will not appear until after the TSTART time (when data is being recorded). Until that time, a status bar will display the progress of the simulation.

Stopping a Simulation: If you wish to stop the simulation you may press the Esc key. The simulation will halt at the current timepoint and save all the data up until that point.

Note, Error Messages: If the simulation status character blinks with a "?" sign, an error has been encountered in the simulation. IsSpice4 places error messages in the Error window, and in a separate file, in order to make them easier to view. This is different than SPICE 2 programs, which place error messages at various points in the output file. When an error occurs, you should look in the error file, called Filename.ERR, for the error message. Filename is the name of the file that you are simulating. Next to the status character is a status field that indicates what analysis is currently being performed. Error messages will be placed under the analysis banner for which they occurred.
The Errors and Status window provides simulation information.

Warnings and Errors are displayed in the Errors Window and stored in the .ERR file.

The Output window functions in a manner similar to the traditional SPICE output file. Data produced by statements (.PRINT analysis) in the netlist will be stored in the output file when IsSpice4 is closed. Data produced by statements that are entered into the Simulation Control dialog's script window will be displayed in the Output window.

Simulation Control Dialog

ICAP/4Rx does not support some of the interactive IsSpice4 features (as indicated). The Simulation Control dialog in ICAP/4Rx will be different.

The Simulation Control dialog is used to control the simulation flow, provide access to past simulation data, and provide access to the interactive stimulus features. The Simulation Control dialog is displayed only after the initial simulation is completed or aborted.

Mode section: The currently active analysis type (last analysis run) is always checked. You can change the active analysis simply by clicking on the desired button. The waveforms for the analysis, if any exist, will be recalled. (The Noise, Disto, and Sens modes are not available in ICAP/4Rx.)

Plots pop-up and Accumulate Plots: The Plots pop-up dialog contains pointers to the available sets of waveform vectors. Waveform vector sets are saved for each of the initial analyses performed. The Accumulate Plots option will determine if a new vector set is created for each succeeding analysis run.

Stimulus Button (Not available in ICAP/4Rx): Invokes the Stimulus Picker dialog, allowing you to select a single part value or model parameter to sweep as stimulus (change) to a design.

Expression Button (Not available in ICAP/4Rx): Invokes the Stimulus Picker dialog, allowing you to select a group of parts or model parameters to sweep.

Measure Button (Not available in ICAP/4Rx): Invokes the Select Measurement Parameters dialog, allowing you to select a portion of the circuit to monitor during parametric changes.

Text can be entered and edited in the ICL Script window.



Command Button (Not available in ICAP/4Rx): Invokes a separate script window, allowing you to run a simulation script. If desired, this is useful for entering ICL commands when the normal script window is being used.

Persistence (Not available in ICAP/4Rx): The number of waveforms displayed in each graph when a parameter(s) is swept.

Use Save Preferences to save the window positions.

Script Atoms: A pulldown menu containing all the available Interactive Command Language (ICL) functions.

ICL Script Window: A text window in which any number of ICL functions can be entered and interactively executed.

Control Buttons (Not available in ICAP/4Rx): The Start, Stop, Pause, Resume, and Abort buttons control the simulation flow.

Saving Windows Positions

Each of the main IsSpice4 windows can be positioned and re-sized. Once you have found a comfortable arrangement for your screen size and resolution, you should save the setup by

selecting the Save Preferences function under the IsSpice4 Edit menu. On the PC, the Auto Size Windows function under the Windows menu will automatically cause the Waveform, Error and Output windows to fill the IsSpice4 window.

Starting, Stopping and Pausing The Simulation

Note: Not available in ICAP/4Rx

The Start, Pause, Resume, and Abort buttons are used to control the IsSpice4 simulation. One or more of these buttons may be gray at a particular time if its function cannot be performed. The Start button clears the Real-Time display and immediately runs the last performed analysis. It does not reload the starting netlist. Abort stops the current simulation and halts all future simulations if any are scheduled.



Note: The Pause button does not need to be pressed in order to interact with the simulator.

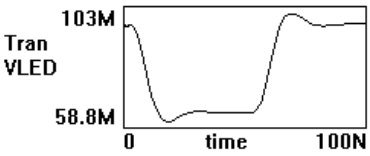
Scaling, Adding and Deleting Waveforms

Before, during or after a simulation, you can alter the Real-Time waveform display by re-scaling, adding, or deleting waveforms. The scales will provide a thumbnail sketch of waveforms, indicating the min. and max. values on the Y axis. Thumbnail sketches save a lot of memory and overhead, as opposed to plotting waveforms in the IntuScope waveform viewer, as is done after simulations.

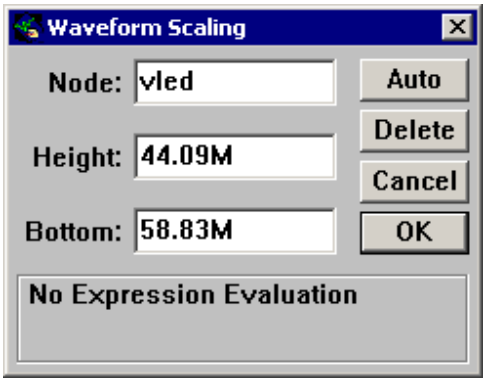
Any saved waveform (described in the next section on Saving Vectors) can be displayed. Initially, vectors from the .PRINT and .VIEW statements will be displayed. Note: only waveforms from the active analysis can be scaled, added, or deleted. For example, if transient is the active analysis, you will only be able to rescale, add, or delete waveform vectors that are saved for the transient analysis.

To rescale all waveforms

- Press <Ctrl>+T on the keyboard. This works at any time for the current analysis.



Double-click on a waveform to bring up the Waveform Scaling dialog



Press Control T or select Auto Scale Waveforms from the OPTIONS menu in order to rescale all of the Real Time waveforms.

To rescale a waveform at any time

- Double-click on the waveform. The Waveform Scaling dialog will be displayed. Click the Auto button to autoscale the waveform or enter the desired scaling.

To delete a waveform

- Double-click on the waveform at any time. Click the Delete button. Select OK. The waveform will be removed the next time the analysis is run.

To add a waveform

- Double-click on an empty area of the display. Enter the vector name into the Node: field. Adjust the scaling. Select OK.

Waveforms specified in the .PRINT statement are displayed using a default scaling set via the .OPTIONS parameters Vscale, Iscale, and Logscale. Waveforms with a .VIEW or ICL view statement will use the scaling values specified on the view line.

Saving Waveform Vectors For Real-Time Viewing

Important Note:
*The SpiceNet schematic entry program automatically saves all of the top-level circuit node voltages, and key device currents and power dissipations. Issuing the *#save all allcur allpow statement is NOT normally necessary!!*

IsSpice4 allows all voltages, currents through components, and computed device parameters to be viewed as waveforms in real-time as long as they have been saved. **Normally, this is done as a quick selection in ICAP/4's Simulation Setup dialog (from the Actions pulldown or SpiceNet's toolbar).** The ICL command **"***#save all allcur allpow**"** is issued in order for all the voltages, currents, and power dissipations to be available. Otherwise, only the vectors listed in the .PRINT/.VIEW statements, or ICL save/view/alias statements will be available. Print Expressions that are made with the alias function are also saved, and will be displayed immediately after the simulation is complete.

As an alternative to the usual way of saving design voltages

- Enter the following statement into the IsSpice4 netlist:

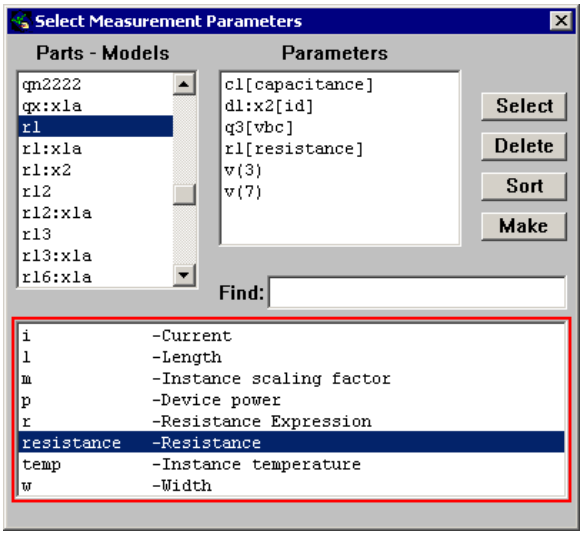
  *#save all

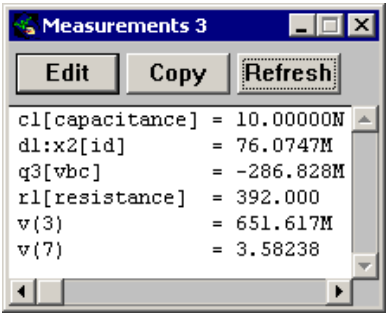
The save allcur and allpow keywords can be used to save all device currents and power dissipations. You can also activate the save function by using the Simulation Setup dialog found in the schematic. However, this can take up a great deal of memory for large circuits. The device and model parameters listed in Appendix B (in the on-line help) can only be saved for viewing with the ICL save function. The desired parameters must be specifically listed, for example:

*#save q1[vbe] m2[gm]

Interactive Circuit Measurements (Not Available in ICAP/4Rx)

The operating point of the circuit can greatly affect the simulation results, especially for the AC analysis. With this in mind, the Measurements dialog can be used to examine the numerical values of different circuit parameters, without schematic intervention. The values for the node voltages and branch currents can be displayed for the operating point of the circuit, or





Measurements dialog

while an analysis is running. For device and model parameters, the operating point values will initially be displayed. They can then be updated at any time by clicking the Refresh button. Note: the real-time waveforms for the selected quantities do not have to be displayed in order for the values to be seen.



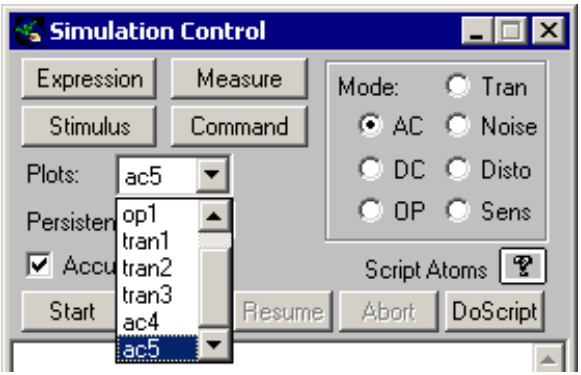
To choose a parameter(s) to measure

- Click the Measure button in the Simulation Control dialog. The Select Measurement Parameters dialog will be displayed.
- Click on the desired topic (main nodes, subcircuit nodes, current branches, or device reference designations). The available list of parameters will be displayed.
- Double-click on the desired parameter(s). When you have chosen all of the parameters that you want, click the Make button.
- Click the Refresh button to see the current values. The next time an analysis is run, the selected values will be updated.

The Copy button places the contents of the Measurements dialog in the Clipboard.

Saving and Viewing Past Simulation Data

A plot name will be given to each analysis during the initial simulation. Some analyses, such as noise and distortion, produce multiple plots. A plot refers to the set of waveform vectors saved with each analysis. The names are listed under the Plots pop-up menu in the Simulation Control dialog. Future analyses will replace the vector set that was most recently simulated unless the "Accumulate Plots" option is checked. For example, if AC and transient analyses are initially run, then the ac2 and tran2 plot vectors will be available. If another transient analysis is run, its data will replace the original tran2 data. If the Accumulate Plots option is checked, a new plot name, tran3, will be created to point to the new transient vector set.



To save the vectors associated with a single analysis

- Check the Accumulate Plots option. As subsequent simulations are run, each set of vectors will be given a new plot name.

To review the data from a past analysis

- Pull down the Plots pop-up and select the desired vector set.

Once a vector is saved, it can be recalled as if it were just simulated. This includes the ability to cross-probe vectors from your schematic entry program and view them in IntuScope.

Note, Memory Usage: After the initial simulation is performed, little or no additional memory will be used unless the Accumulate Plots option is checked. Using the save all allcur allpow option along with the Accumulate Plots option, can cause large amounts of memory to be used.

Sweeping Circuit Parameters (Not Available in ICAP/4Rx)

The interactive stimulus feature can be accessed any time, even when a simulation is running.

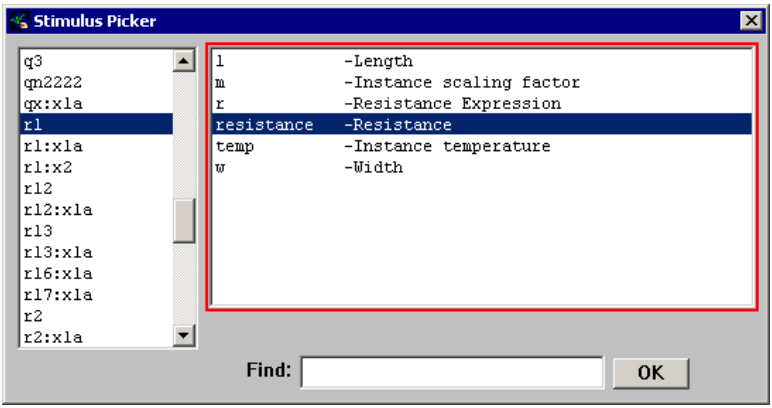
The interactive stimulus feature of IsSpice4 allows virtually any circuit parameter to be changed at any time, and a simulation to be immediately rerun.

To select a device/model parameter for sweeping

- Click the Stimulus button in the Simulation Control dialog. The Stimulus Picker dialog will be displayed.



Stimulus Picker dialog



- Click on the desired reference designation or model name on the left. The available list of parameters to change will be displayed on the right.
- Double-click on the desired parameter or click on the parameter and click OK.

The Interactive Stimulus dialog will be displayed. Note: The find field can be used to find a particular entry in lieu of scrolling.

An asterisk in the Set button indicates that the circuit has not been simulated with the displayed value.

Interactive Stimulus dialog



The current value of the parameter will be displayed in the Interactive Stimulus dialog.

To set a new parameter value

- Either type the desired value or use the arrows.

The arrows at the center will change the value slightly while the arrows on the ends will change the value greatly. The left arrow moves the value down while the right arrows move the value up. Each arrow changes the value by a difference of one order of magnitude, thus providing a total control range of 5 orders of magnitude up or down.

To change the range of magnitudes that the arrows control

- Click on the center dot. You can then move the dotted box to a new set of magnitudes.
- Click the dot to go back to the Interactive Stimulus function.



To run an analysis with the new parameter value

- Click the Set button.

You may have as many Stimulus dialogs open as you like.

When the parameter value is changed, the Set button will have an asterisk, which indicates that a simulation with this new value has not yet been run. Clicking the Set button runs the last analysis with the new value.

To hand-tweak a parameter value

- Check the Always button. Change the parameter value by holding down one of the Stimulus dialog arrows.

If the Always button is checked, the analysis will be run as soon as the value is changed. If the mouse button is held down, the parameter will be changed and a new analysis will run as soon as the old analysis is completed. In this way, it is possible to control a circuit variable and watch the waveforms change. However, is simulation run times are longer than several seconds, the changes in waveforms and selected measurement values will be delayed.

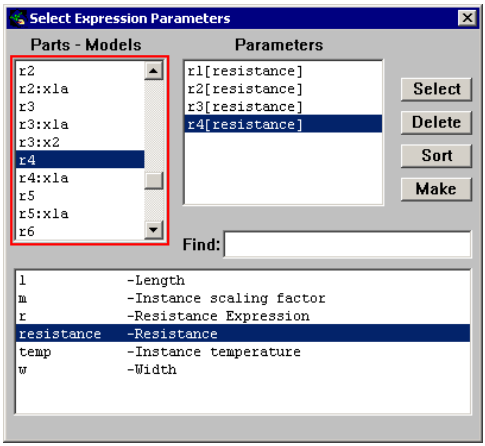
Sweeping Groups of Parameters (Not Available in ICAP/4Rx)

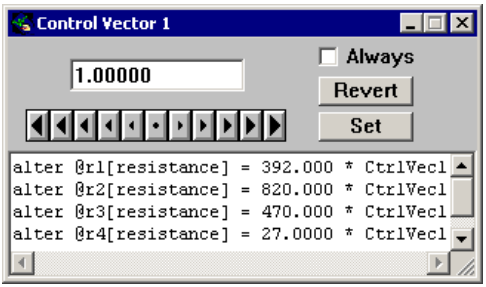
The Expression dialog works in a manner that is similar to the Interactive Stimulus dialog. However, several circuit variables may be swept in tandem.

To select a group of device/model parameters for sweeping



- Click on the Expression button in the Simulation Control dialog. The Select Expression Parameters dialog will be displayed.
- Click on the desired reference designation or model name on the left. The available list of parameters to change will be displayed at the bottom of the dialog.
- Double-click on the desired parameter(s). Then click the Make button.





Interactive Expression dialog

The Interactive Expression dialog will be displayed. Note: You may choose any combination of parameters.

The Make button will construct the Interactive Expression dialog with each circuit parameter multiplied by a control vector, for example, CtrlVec1. When the CtrlVec1 value is changed, all of the circuit parameters will be changed based on this value using the ICL Alter function.

To set a new CtrlVec value

- Either type the desired value or use the arrows.

The arrows will behave in a manner similar to those in the Interactive Stimulus dialog.

To run an analysis with the new CtrlVec value

- Click the Set button.

When the CtrlVec value is changed, the Set button will have an asterisk in it, indicating that a simulation with this new value has not yet been run. Clicking the Set button runs the last analysis with all of the Alter variables set to the new value.

In other words, the Interactive Expression dialog will run all of the Alter statements, like a simulation script, BEFORE running the analysis.

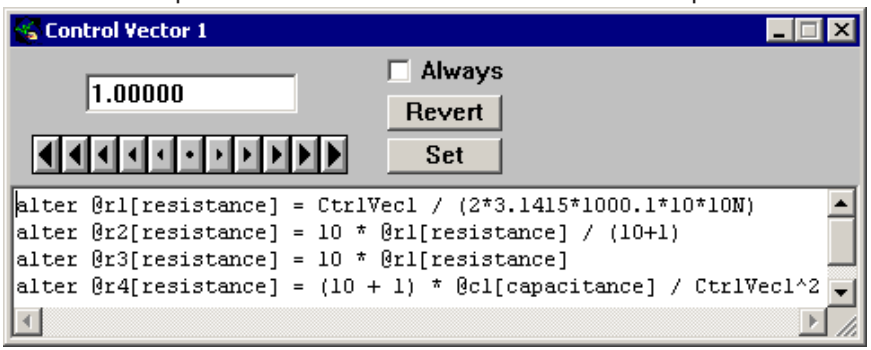
To hand-tweak all of the parameters

- Check the Always button. Change the CtrlVec value by holding down one of the Expression dialog arrows.

The Always button option works in a manner similar to the one in the Interactive Stimulus dialog.

Note: The latest value assigned to a component parameter will remain that value, even once all the aforementioned dialog boxes are closed. Only re-running a simulation from the schematic, in the usual way, will revert components back to their true original value.

In addition to the ability to sweep a group of parameters, the circuit parameters may be independent or functions of other circuit variables. For example, in the Expression dialog shown below, the first resistance parameter is a function of an equation, while the second is a function of the first resistance value. The capacitor value is a function of the CtrlVec1 squared.



Virtually any combination of circuit variables can be swept in this manner, giving you the ability to thoroughly explore your design.

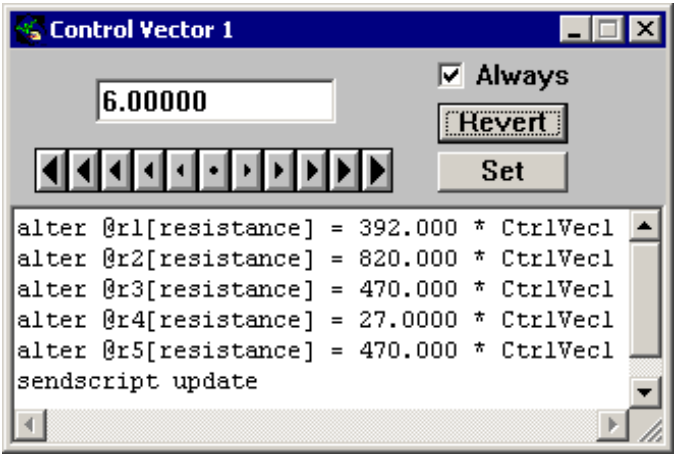
Adding An ICL Script To A Sweep

Apart from the usual easy way of sweeping component values and temperature in SpiceNet using the Alter icon, an ICL command can be placed in the Interactive Expression dialog.

Any ICL command can be entered into the Expression dialog.

This gives you the ability to run multiple analyses, alter multiple sets of parameters, and easily build curve families. For example, by adding the Sendscript update command, the already plotted vectors will be updated in IntuScope each time the CtrlVec1 is changed, automatically building a curve family.

Sendscript update in IsSpice4 sends the update command to IntuScope



Important Note: For this to work IntuScope must already be opened, and you need to plot at least one vector you are interested in. Also the contents of the Interactive Expression dialog will run BEFORE the analysis, the sendscript update will be for waveforms from the PREVIOUS analysis.

Scripting: Introduction to ICL

See the ICL chapter in this manual for more information.

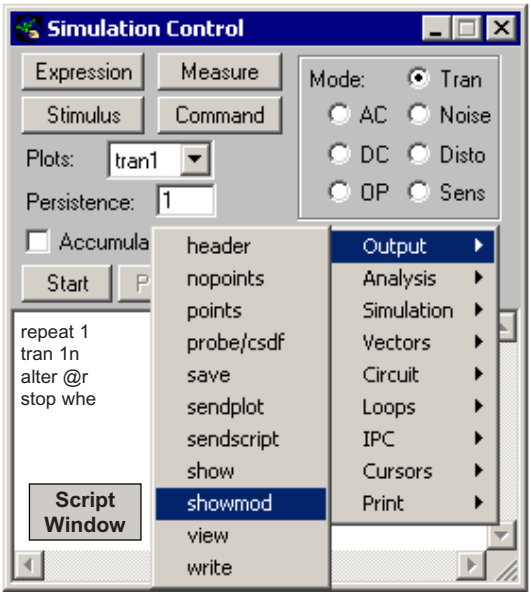
The DoScript button in the Simulation Control dialog is used to run the Interactive Command Language functions that have been typed into the Simulation Control dialog's Script window. ICL functions can also be entered in the IsSpice and IntuScope Command windows, Expressions window, or the input netlist's control block. The Script Atoms pop-up contains all of the available ICL functions, which include most of the traditional SPICE analysis functions.

Some of the tasks you can perform include:

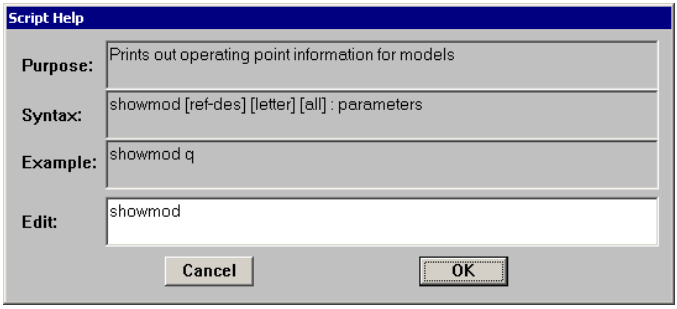
- Interactively run different analyses
- Put static reference data points on a graph (points)
- Set *Simulation Breakpoints* (stop)

Script Atoms pop-up dialog

Scripts may be run individually or in groups. They can also be saved to a text file for later use.



Help dialog for the Show function



The text in the Script, Output, and Help windows can be edited (cut, copy, paste) using the keyboard control keys (^x, ^c, ^v).

- Display detailed operating point information (show/showmod)
- Set up simulation loops to create curve families

To obtain help on an ICL function

- Select the Script Atoms pop-up and select the desired function.

When a function is selected, a help dialog will be displayed. All of the information in the fields of the dialog can be copied to the Edit: field at the bottom. The OK button causes the Edit: field contents to be copied to the script window at the cursor position.

To run a simulation script

- Click the DoScript button. The contents of the script window will be executed.

Viewing Waveforms In More Detail

There are two methods to place these real-time waveforms inside IntuScope. The first method allows you to control IntuScope from within the IsSpice4 environment by sending ICL scripts to IntuScope using the sendscript command. This enables you to modify real-time display waveforms as desired, then send them over to IntuScope for further study without leaving IsSpice4. Note: IntuScope must be open for the scripts to run.

The sendscript syntax is covered in detail in the ICL chapter 11.

To plot a real-time waveform in IntuScope with IsSpice4

- Click in the ICL Script window to activate it and type "sendscript plot" *name*, where *name* is the name of the vector you want to send.
- Click the DoScript button.

The second of the two above methods links IntuScope directly to the "Active IsSpice Simulation," after the run is complete. This essentially connects the IsSpice4 Simulation Control and IntuScope Add Waveform Dialog together. You can see at a glance that this link is active if you can click on the "All Test Pts" button at the bottom left of IntuScope's Add Waveform Dialog. This button allows you to plot all test points' real-time waveforms with one click. Also, the Add Waveform Dialog makes it easy to plot any waveform simply by selecting it from a list. Note: IntuScope only has access to all of your saved real-time circuit vectors if IsSpice4 is still running.

Analysis Types

Analysis Summary

Listed below are the various types of analyses that IsSpice4 can perform. They are listed under the general type of analysis to which they apply. Each line contains the IsSpice4 keyword, shown on the left, and a brief explanation. Note that all control statements in the main netlist begin with a dot, while control statements in the ICL block or in the Simulation Control script window do not.

ICAP/4Rx Note: The .FOUR, .NOISE, .DISTO, .TF, .SENS, Monte Carlo, Optimization, and Failure analyses and Simulation Templates are NOT available in ICAP/4Rx.

DC Analyses

DC...DC Analysis - DC sweep of an independent voltage or current source
OP...DC Operating Point - Small-signal bias solution
TF...Transfer Function - DC transfer function with input/output impedances
SENS...Sensitivity Analysis - DC small-signal sensitivity

AC (Small-Signal) Analyses

AC...AC Analysis - Frequency response/Bode plot
NOISE...Noise Analysis - Output, equivalent input, and component noise
DISTO...Distortion Analysis - Harmonic/Intermodulation distortion
PZ...Pole Zero - Pole/Zero transfer functions
SENS...Sensitivity Analysis - AC small-signal sensitivity*

Transient Analyses

TRAN...Transient Analysis - Nonlinear time domain response
FOUR....Fourier Analysis - Harmonic analysis with THD

Temperature Analyses

OPTIONS TEMP...Circuit and element temperature variations

ICL - Interactive Command Language

User-defined command scripts that drive IsSpice4. The ICL includes over 60 different commands and functions

Simulation Templates - ICL Command Scripts

*Sensitivity (Time, AC, DC) , RSS, EVA (Extreme Value), and Worst Case, running for the Transient, AC, DC, and Operating point analyses

Code Models And Analysis Types

Code models that use the event-driven simulator in IsSpice4 (digital, real), cannot be used in an AC analysis.

There are 2 basic types of code models that are supplied with IsSpice4; analog and event-driven. A code model may be classified by looking at its input and output nodes, which may be of the analog or event-driven type. Event-driven node types can be further subdivided into digital, real, integer, and user-defined. A hybrid model is one that uses two or more node types. Event-driven models are simulated by an event-driven algorithm. The analog and hybrid models that use analog nodes are simulated by the SPICE 3 algorithm. Both algorithms are included in IsSpice4.

Analog code models should only be used in the operating point, DC sweep, AC and transient analyses. Event-driven code models, including hybrid models, can only be used in operating point, DC sweep, and transient analyses. There is no provision for using AC analysis with event-driven code models. Other analysis types, such as noise or distortion, are not supported at this time.

ICL - Interactive Command Language

See Chapter 11 for more information on ICL.

IsSpice4 contains a scripting language that includes functions for simulation control (such as breakpoints and loops), functions for output control (such as **print, show** and **alias**), and all of the standard analysis operations.

DC Operating Point Analysis

.OP will cause a DC operating point to be printed.

Produces the operating point of the circuit, including node voltages and voltage source currents.

The DC analysis portion of IsSpice4 determines the quiescent DC operating point of the circuit with inductors shorted and capacitors opened. A DC analysis, known as the “Initial Transient

Use the ICL Show commands to get additional operating point information.

Solution", is automatically performed prior to a transient analysis to determine the transient initial conditions. A DC analysis, known as the "Small Signal Bias Solution", is performed prior to an AC small-signal analysis to determine the linearized, small-signal models for all nonlinear devices. It should be noted that these two operating point calculations may be different, depending on the DC and transient stimulus used.

DC Small Signal Transfer Function (Not Available in ICAP/4Rx)

The .TF statement controls the transfer function analysis.

The .TF function produces the DC value of the transfer function between any output node and any input source, along with the input resistance looking into the circuit at the source, and the output resistance looking into the output node.

This analysis computes the small signal ratio of the output node to the input source and the input and output impedances. Any nonlinear models, such as diodes or transistors, are first linearized based on the DC bias point, and then the small signal DC analysis is carried out.

DC Sweep Analysis

See the .DC syntax in Chapter 10 for more information.

See the .PRINT statement for more information on getting data out of the DC sweep analysis.

Produces a series of DC operating points by sweeping one independent source, or two sources in a nested loop.

The .DC function is a special subset of the DC analysis feature. It is used to perform a series of DC operating points by sweeping voltage and/or current sources and performing a DC operating point at each step value of the source(s). At each step, the DC voltages, currents, and computed device/model parameters can be recorded. The .DC line defines which sources will be swept, and in what increments. One or two sources can be involved in the DC sweep. If two are involved, the first source will be swept over its range for each value of the second source. This option is useful for obtaining semiconductor device output characteristics or calculating load lines.

Sensitivity Analysis (Not Available in ICAP/4Rx)

Produces the Operating Point, DC, AC, and Transient sensitivities of any output variable with respect to all circuit parameters, or, the sensitivities of any circuit parameter with respect to any output variable.

See Chapter 10 for more info on sensitivity analysis.

There are two sensitivity analysis approaches; traditional SPICE and Simulation Templates. Sensitivity is useful when trying to find worst-case circuit operation. By finding the most sensitive components and moving their values accordingly, the circuit's performance can be evaluated. The traditional SPICE form of the sensitivity analysis uses the direct approach [3-1] to support sensitivity calculations for the DC and AC analyses. The DC sensitivity is with respect to the DC operating point. IsSpice4 calculates the difference in an output variable, either a node voltage or a branch current, by perturbing each parameter of each device independently. Since the method is a numerical approximation, the results may demonstrate second-order effects in highly sensitive components, or may fail to show very low but nonzero sensitivity. Since each variable is perturbed by a small fraction of its value, zero-valued parameters are not analyzed. The output, consisting of the sensitivity of all circuit parameters (values and model parameters) with respect to a named voltage or current, is placed in the IsSpice4 output file.

*See **Simulation Templates** in this chapter for more info on sensitivity, RSS, EVA, and worst case analysis.*

IsSpice4 supports a more powerful sensitivity analysis using Simulation Templates. AC, DC, Transient, and OP related sensitivities may be obtained for large parameter perturbations using this method. In addition, this version is more flexible and allows more sorting and output options. For example, you can get the sensitivity of any circuit parameter with respect to any output measurement (maximum, minimum, or rise time for any voltage, current, power dissipation waveform, etc.) as well as the opposite; the sensitivity of any output measurement with respect to any circuit parameter. RSS, EVA, and Worst Case options are also available when using Simulation Templates. This is the preferred method for sensitivity analysis.

AC Analysis

Generates a frequency response/Bode plot of the circuit. Magnitude, phase, real, or imaginary data is produced.

The AC analysis in IsSpice4 computes the small signal response of the circuit. Output variables are recorded as a function of frequency.

The .AC statement controls the AC analysis.

Before the AC analysis is performed, IsSpice4 first computes the DC operating point of the circuit. It then determines the linearized, small-signal models for all of the nonlinear devices in the circuit, based on this operating point. The resultant linear circuit is then analyzed over the specified range of frequencies. Therefore, it is important to establish the proper DC circuit biasing in order for the AC analysis to produce useful data. For example, biasing an op-amp in its linear range will give different AC results than if the op-amp is saturated.

DC Bias Note: It should be noted that the small-signal bias point is determined by the DC values on the independent source rather than the initial transient signal generator values.

See the .PRINT statement for more information on getting data out of the AC analysis.

The desired output of an AC small-signal analysis is usually a transfer function (voltage gain, transimpedance, etc). If the circuit has only one AC input (normal case), then that input is traditionally set to unity magnitude and zero phase. By doing so, the output variables have the same value as the transfer function. For example, if the input is a voltage source with magnitude 1, then the output node voltages would equal gain: Gain = Vout/Vin, which equals Vout, with Vin = 1.

Although the AC analysis performs a sinusoidal steady-state analysis, it should not be confused with a transient (time domain) analysis using a large signal SINE wave. The AC analysis is a small-signal analysis where all non-linearities are linearized. For instance, if the DC biasing of a transistor gain stage produces a gain of ten, then the gain will remain ten no matter what the input. If 1 is the input, then 10 is the output.

If 100 is the input, then 1000 is the output. The gain is linearized. Under nonlinear conditions, however, the gain of the transistor will roll off as the input is increased. The “VName 1 0 SIN.....” stimulus is only used for time-domain analyses, and should not be confused with the “Vname 1 0 AC 1” AC stimulus.

See the voltage source syntax in Chapter 8 for information on AC analysis stimulus.

Frequency Mixing Note: The AC analysis is a single frequency analysis. Only one frequency is analyzed at a time. Therefore, circuits performing signal mixing will not benefit from the AC analysis. In order to see frequency mixing, you will have to run a transient analysis and convert the output waveforms into the frequency domain using a Fourier transform.

Noise Analysis (Not Available in ICAP/4Rx)

Produces the output and equivalent input noise over a specified range of frequencies, as well as the noise generated by active components and resistors.

The .NOISE statement controls the noise analysis.

The noise analysis computes the integrated noise contributions for each noise generating element in the circuit over the frequency range that is specified in the Noise statement. It also calculates the level of input noise from the specified input source, which is required to generate the equivalent output noise at the specified output node.

The calculated value of the noise corresponds to the spectral density of the circuit variable. After calculating the spectral densities, the noise analysis integrates these values over the specified frequency range in order to determine the total noise voltage or total noise current. The particular output variables are defined by the Noise analysis statement.

See the .PRINT statement for more information on getting data from the noise analysis.

Noise data is stored in the output file in two forms. One is for the noise spectral density curves, INOISE and ONOISE, and the other is for the total integrated noise over the specified frequency range. All noise voltages/currents are in squared units (V^2/Hz and A^2/Hz for spectral density, V^2 and A^2 for integrated noise) to maintain consistency and prevent confusion.

The types of noise contributions are thermal noise from resistors, whether they are discrete or internal ohmic semiconductor resistances, and shot and flicker noise from semiconductors. Each noise source is assumed to be statistically un-correlated to the other noise sources in the circuit. Each noise source value is calculated independently. The total noise is the RMS sum of the individual noise contributions.

Distortion Analysis (Not Available in ICAP/4Rx)

Distortion analysis is useful for investigating small amounts of distortion that are normally unresolvable in the transient analysis.

Produces small signal steady-state harmonic and intermodulation distortion data.

The distortion analysis computes the steady-state harmonic and intermodulation products for small input signal magnitudes. Distortion analyses can be performed using linear devices and the following semiconductors; diode, BJT, JFET, MOSFET and MESFET. If there are switches present in the circuit, the analysis will continue to be accurate if the switches do not change state under the small excitations that are used for distortion calculations.

The .DISTO statement controls the distortion analysis.

In the distortion analysis, a multidimensional Volterra series analysis is solved using a multidimensional Taylor series to represent the non-linearities at a specific circuit operating point. Terms up to the third order are used in the series expansions. One of the advantages of the Volterra series technique is that it computes distortions at mix frequencies symbolically (i.e. n F1 ± m F2). It is possible, therefore, to obtain the strengths of distortion components accurately even if the separation between them is very small. The disadvantage is, of course, that if two of the mix frequencies coincide, the results are not merged together and presented. However, this could be done as a post-processing step in the IntuScope program. You will have to keep track of the mix frequencies and add the distortions at coinciding mix frequencies together.

Pole-Zero Analysis

Produces the poles and/or zeros of a transfer function.

The .PZ statement controls the pole-zero analysis.

The pole-zero analysis computes the poles and/or zeros of a small-signal AC transfer function. The program first computes the DC operating point and, like the AC analysis, determines the linearized, small-signal models for all of the nonlinear devices in the circuit. The circuit is then analyzed to find the poles and zeros. The pole-zero analysis works with resistors, capacitors, inductors, linear-controlled sources, independent sources, BJTs, MOSFETs, JFETs, MESFETs, and diodes. Transmission lines are not supported.

Two types of transfer functions are allowed, VOL and CUR: VOL represents (output voltage)/(input voltage) and CUR represents (output voltage)/(input current). These two types of transfer functions cover all cases. For each transfer function, you can find the poles, zeros, or both. This feature is provided mainly because if there is a non-convergence in finding poles or zeros, then at least the other can be found. The input and output ports are specified as two pairs of nodes. Thus, there is complete freedom regarding the output and input ports and the type of transfer function. The results of the pole-zero analysis may be found in the output file.

The method used in the analysis is a suboptimal numerical approach. For large circuits, it may take a long time, or it may fail to find all of the poles and zeros. For some circuits, particularly those with active devices and op-amp macro models, the method may become lost and find an excessive number of poles and zeros.

Transient Analysis

Runs a nonlinear time domain simulation.

The transient analysis computes the circuit response as a function of time over any time interval. Output data, including node voltages and voltage source currents, can be recorded using the .PRINT or .PLOT statements. During a transient

analysis, any number of independent sources may have active time-varying stimulus signals.

The .TRAN statement controls the transient analysis.

The transient time interval is specified on a TRAN control line using the parameters TSTEP, TSTOP, TSTART, and TMAX to control the data printout step, total analysis time, start of data recording time, and maximum internal timestep, respectively.

In earlier versions of IsSpice, two techniques were used to control the simulation timestep: iteration count and truncation error (default). In IsSpice4, the iteration count method has been eliminated.

Transient Initial Conditions

The initial voltages and currents are automatically determined by a DC operating point analysis called the "Initial Transient Solution." This operating point is performed before the transient analysis begins, and may be different than the small-signal bias solution. All sources that are not time-dependent (for example, power supplies) are set to their DC value, while sources that are time-varying are set to their initial values.

UIC (use initial conditions) is an optional keyword in the .TRAN statement that causes IsSpice4 to skip the initial transient solution that is normally performed prior to the transient analysis. If this keyword is included, IsSpice4 uses the values that have been specified using "IC =" values on the various elements, and .IC statements, as the sole source for initial conditions. The transient analysis will start with these values. The first set of valid node voltages will be placed in the output file under the "Initial Transient Solution" banner in order to provide information on the initial state of the transient analysis.

See the .IC statement in Chapter 10 for more information.

How IsSpice4 Runs A Transient Analysis

IsSpice4 accurately computes transient events via a variable timestep control algorithm. During a simulation, the rate at which the time progresses will vary in order to maintain a specific

accuracy. For example, when capacitor voltages and inductor currents are changing very little, the program will take larger timesteps. If the timesteps were fixed at the shortest possible timestep, then the simulation could run hundreds or even thousands of times longer than necessary. The use of a variable timestep is one of the major breakthroughs that SPICE has brought to the world of circuit simulation.

The "Timestep Too Small" error trap is set to 10^{-9} times TMAX.

The default timestep selection algorithm uses an estimate of the Local Truncation Error (LTE) of integration. The LTE is the estimate of the error between the real answer and the answer that is produced by the current integration method, either Trapezoidal or Gear. When the LTE is too large, the timestep is reduced. If the timestep is reduced below 10^{-9} times the maximum timestep, the simulation will be aborted. The error message "Timestep Too Small" will be reported. The maximum time allowed can be altered by adjusting the TMAX parameter in the .TRAN control statement. When the LTE is determined to be too small, the timestep is allowed to increase up to the maximum time step. The LTE is overestimated by a factor of 7 for timestep increases, thereby causing a hysteresis in the timestep control.

TRTOL in the .OPTIONS control statement sets the LTE overestimate. The default of TRTOL=7 was selected in order to give the fastest simulation time for a number of test cases. Changing TRTOL is not recommended.

RELTOL controls the simulation timestep.

RELTOL is the .OPTIONS control parameter that sets the LTE. Note: VNTOL, CHGTOL and ABSTOL will also affect the selection, however, since only the largest of these error terms is used for the timestep change, RELTOL is usually the dominant parameter.

Output Data And Aliasing

In IsSpice4, output is recorded at each TSTEP interval, which is specified in the .TRAN control statement. This time is not the same as the computational timestep. The computation can be proceeding at either shorter or longer intervals than TSTEP. To

get the output values, the program uses linear interpolation of the data to produce a uniformly spaced output for each TSTEP. The default linear interpolation can be changed to a higher order using the .OPTIONS INTERPORDER parameter.

TSTEP in the TRAN statement must be small enough to resolve the highest frequencies.

The maximum frequency that can be resolved in the simulation output data is set by the Nyquist criteria at 1/(2*TSTEP). If higher frequencies are present in the simulation, perhaps due to oscillation or ringing, they will be viewed incorrectly as lower frequencies when the data is plotted. The simulation, however, proceeds at the timesteps that are needed to resolve the higher frequencies, even if the recorded data will alias the real response.

Use the TMAX parameter in the TRAN statement to reduce the maximum time step.

The maximum timestep can be too long to resolve even transient driving functions. The transient signal generators in IsSpice4 do not make contributions to Local Truncation Error, LTE. A sine wave, for example, could go through a large portion of a cycle or even several cycles between timesteps. The linear interpolation algorithm would lead to inaccuracies or even nonsense if this condition were allowed. To counteract the problems associated with large timesteps and aliasing, you should use the VSECTOL option. The argument of VSECTOL lets the largest error in volts-seconds possible between time steps.

VSECTOL reduces the time step if the product of the absolute value of the error in predicted voltage and the time step exceeds the VSECTOL specification. Using VSECTOL to control the time step produces higher accuracy during the turn-off transition and uses less computational resources when there is no switching activity.

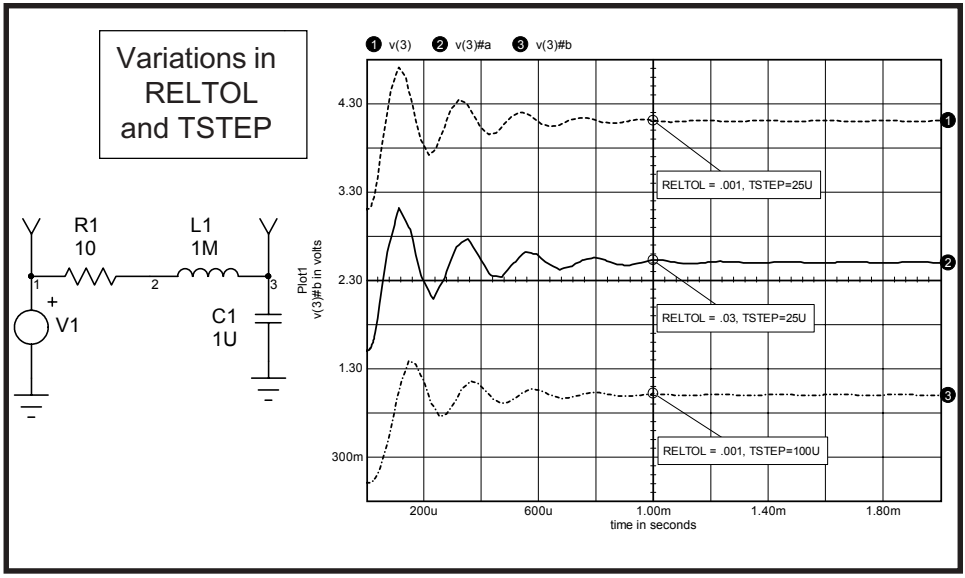
Changing The Simulation Accuracy

Increasing RELTOL can dramatically increase simulation speed. When circuits become very complex, the highest frequency at any given time will control the timestep. If accuracy related to that activity is less important, then the overall simulation accuracy will not be compromised by increasing RELTOL. For a stable simulation, the steady-state circuit values will not be

changed by increasing RELTOL. Increasing RELTOL to greater than .03 will usually have adverse effects on simulation stability, making it impossible to arrive at a steady-state solution. If you set VSECTOL then you can effectively change the time step control to VSECTOL, increasing RELTOL to .01 and disable model bypass by setting BYPASS=0.

Increase RELTOL to .01 to speed the simulation and eliminate "Timestep Too Small" errors.

For Example:
The figure below illustrates the effect of timestep control on simulation results. All traces have the same y-scaling and all of the simulations used trapezoidal integration. The top trace shows the true results. The second trace illustrates the degradation in simulation stability, which is caused by increasing RELTOL to .03. The third trace illustrates the aliasing caused by making the output resolution too coarse.



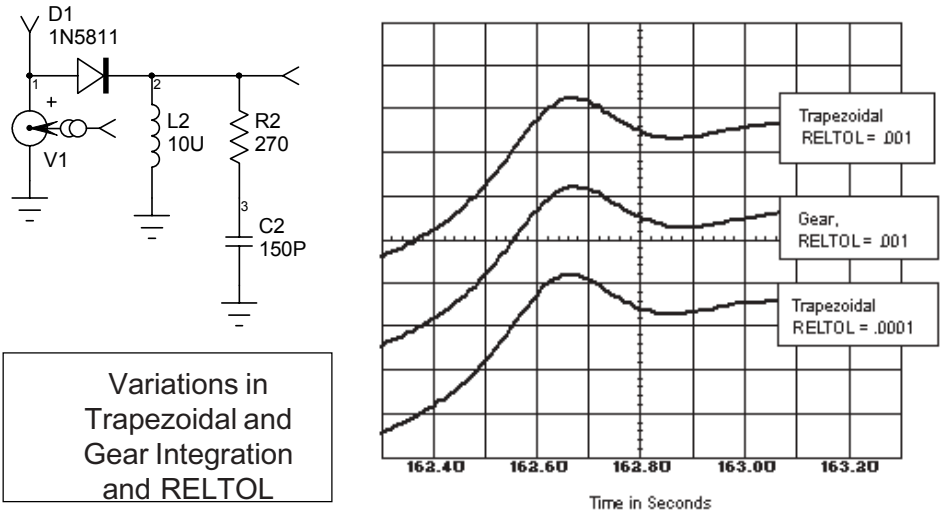
Simulation Stability

The transient simulation uses variable timesteps and nonlinear equations to solve for circuit values. Numerical solution of these circuit equations introduces potential instability in the mathematical description. The combination of variable timesteps

Gear Integration can be selected using the .OPTIONS METHOD=GEAR

and nonlinear circuit equations has no known stability criteria. Ringing or oscillation can result from the degradation in stability, which is caused by numerical integration and its associated errors. Limit cycles have been observed in many simulation outputs at very small levels. In some cases, the limit cycles may become significant and it will be up to the designer to distinguish between numerical artifacts and true circuit behavior.

If the output is sampled at a high enough frequency, then reduction in RELTOL will produce more accurate results. RELTOL is small enough when further reductions fail to produce significant changes in data.

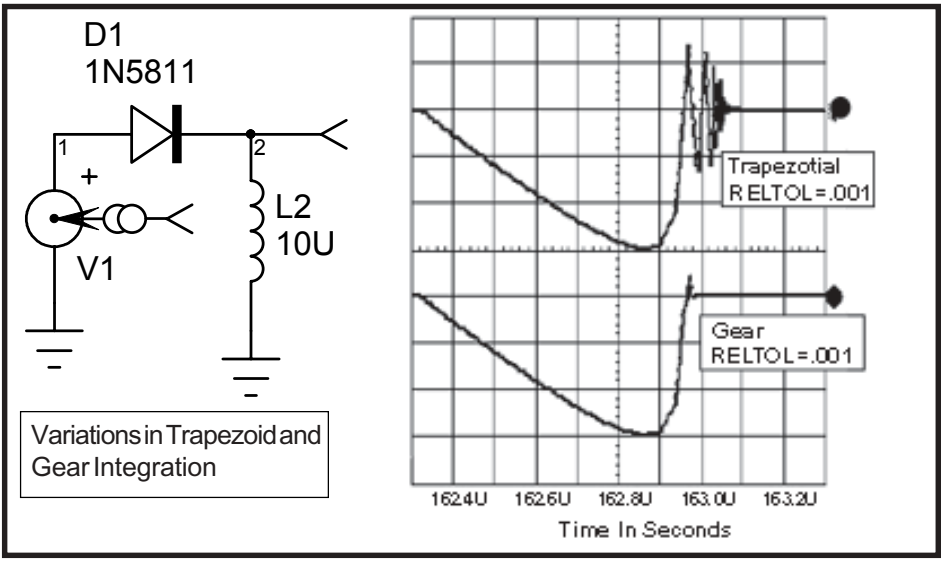


Variations in Trapezoidal and Gear Integration and RELTOL

Changing from the default trapezoidal integration to the Gear method will frequently improve stability when inductors and switches such as diodes are present. The figure above illustrates the increased accuracy that is provided by the Gear integration method for the same RELTOL. Trapezoidal integration produced the same results in less time when RELTOL was reduced to .0001. In larger circuits, the smaller value of RELTOL will frequently result in “Timestep Too Small” errors.

The next figure uses the same circuit as the figure shown above, except the damping R-C network has been removed. This is a

common configuration in power circuits. The high frequency ringing will cause small time steps and use excessive computational time on an unimportant performance parameter. Increasing RELTOL with the GEAR integration produces errors in the direction of a more stable numerical solution, while trapezoidal integration tends to produce a less stable solution. It is for this reason that GEAR integration with a large RELTOL provides superior results for power circuitry.



Variations in Trapezoid and Gear Integration

Fourier Analysis (Not Available in ICAP/4Rx)

Produces the magnitude and phase vs. frequency response for the DC and first 9 harmonics, plus the total harmonic distortion.

The Fourier analysis determines the DC component plus the first 9 AC frequency and phase components. Also, the normalized frequency and phase are printed along with the total harmonic distortion. Several output variables may be listed for each Fourier analysis that is performed.

The total harmonic distortion is the square root of the sum of the squares of the second through ninth normalized harmonics times 100, and expressed as a percent,

$$\%THD = \left[\sqrt{\sum_{m-2}^{9} \left(\frac{R_m}{R1} \right)^2} \right] * 100$$

Care must be taken when performing a Fourier analysis. Since IsSpice4 is actually performing a **Discrete Fourier Transform,** all of the problems associated with taking a DFT on a non-periodic waveform are applicable.

A more flexible version of the Fourier analysis is available through the use of the ICL Fourier function and in the IntuScope waveform processing program. This version allow for a variable number of harmonics and complex expressions, as opposed to being limited to node voltages.

Temperature Analysis

IsSpice4 allows you to vary the temperature of the circuit or a particular element.

See the .OPTIONS TEMP parameter in Chapter 10 for more info on changing the circuit temperature.

IsSpice4 simulates circuits at a nominal temperature of 27 deg C (.OPTIONS TEMP=). The temperature at which device model parameters are calculated is also set to a default of 27 deg C (.OPTIONS TNOM=). Both of these values can be changed. In addition, the temperature at which model parameters were calculated, as well as the simulation temperature for an individual device, can also be set. This allows IsSpice4 to simulate temperature gradients, as well as a "hot" device. Global temperature changes are performed with .OPTIONS parameters, while individual device temperatures are set directly on the device call line or in the .model statement.

See the Getting Started book for more info on temperature sweeps.

Temperature dependent support is provided for resistors, diodes, JFETs, BJTs, and level 1, 2, 3, and 4 MOSFETs. MOSFETs that use the BSIM models have an alternate temperature dependency scheme that adjusts all of the model parameters before they are input to IsSpice4. For details on the BSIM temperature adjustment, see [3-2,3].

The equations that describe the temperature dependence of the various model parameters can be found under the syntax of the appropriate element.

Simulation Templates (Not Available in ICAP/4Rx)

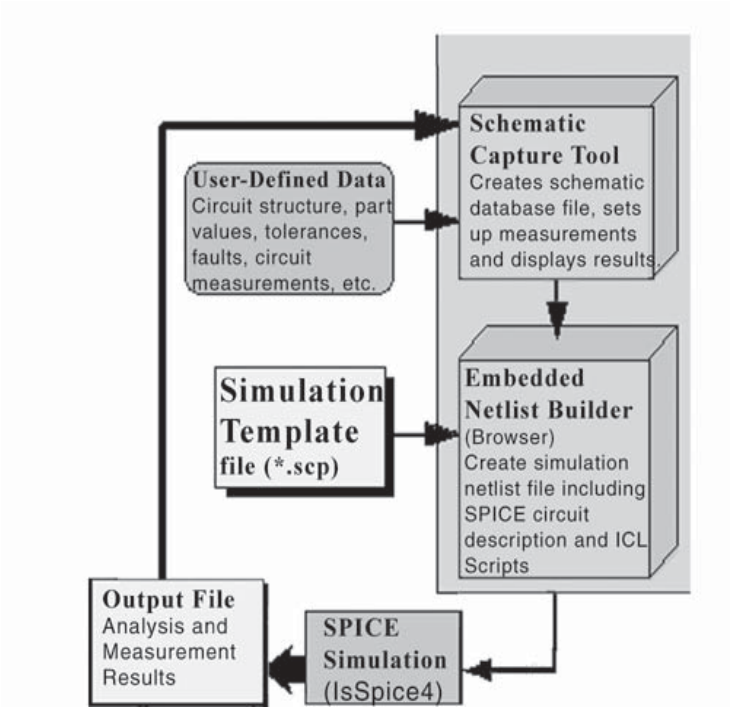
IsSpice4 allows you to create and run advanced analyses using a series of ICL commands in a script file, or the usual simulation control dialog in SpiceNet.

ICL Scripts are set up using ICAP/4 Simulation Control Dialog's Measurement Wizard (in the Measurements tab).

SPICE simulators operate on a netlist and perform a standard set of simulations; AC, DC, Transient, etc. Normally these analyses are performed once and then control is passed back to the user. By adding a script based control language, you can command the simulator to perform multiple analyses as well as process the simulation results. This automation can result in huge time savings and the elimination of many repetitive manual operations. The ICL script features of IsSpice4 give you this capability. What's been missing, until now, is the ability to create new analysis types.

The analysis types that have been most often requested are based on transient sensitivities: RSS (Root Summed Square), EVA (Extreme Value Analysis), and worst case analysis. In theory, each of these analyses can be performed using scripts; however, the scripts would have to be specialized for each circuit. Simulation Templates were invented by Intusoft to automatically integrate ICL scripts with the netlist building function in the schematic capture tool, in order to enable a variety of design verification analyses.

Simulation Templates are ICL scripts that have additional embedded instructions that tell the schematic netlister function where to insert design specific information into the ICL script stream. Template files are text files with a .SCP extension. They are located in the Script folder under SPICE8 (by default).



As shown in the figure, the schematic netlist builder combines the circuit description (standard SPICE syntax) with user-defined measurements. The user-defined measurements perform automated waveform analysis (previously done manually in the IntuScope post processing tool). The measurements are specified in the ICAPS Simulation Control dialog's Measurements tab. When a Simulation Template based analysis is requested, the schematic reads the template .SCP file and uses the embedded instructions to construct an ICL script specific for the design. The resulting IsSpice4 netlist, which contains the circuit description and complete ICL script, is then sent to IsSpice4. The results of the simulation are placed in the output file. They can be viewed with IsEd, or the Results dialog within the ICAPS Simulation Control dialog.

See Chapter 11 for more information on ICL scripts.

Simulation Templates can be easily edited to create custom report formats and even to modify the analysis based on your special needs. Extensions to optimization, what-if and sneak circuit analysis are possible. Templates that perform Worst Case, RSS, EVA, and Sensitivity measurements using OP, AC, DC and Transient analysis are included with IsSpice4.

Expanding these traditional analyses using Simulation Templates requires single valued measurements (i.e. rise time, maximum value, average value, etc.) to be available for the perturbation (sensitivity) analyses that are performed. The user-defined

measurement capability is used to make these easily applicable to analyses that produce vector data, such as a transient analysis. For example, we can speak of the sensitivity of the output's rise time with respect to the change of a parameter value. The sensitivity of the entire output vector would be possible to compute, but we couldn't mathematically identify the best output vector - while we could identify characteristics such as the smallest rise time or the greatest standard deviation. These scalar results are needed in order to make decisions about their relation to parameter values, and to use that decision to find parameter values that correspond with a goal; for example, to make a best or worst result.

For more detail on Simulation Templates, including how they work and instructions on how to create your own scripts, please see the on-line HTML based help. Access to this help is available from the schematic's on-line help, IsSpice4's on-line help, and the Intusoft web site.

References

[3-1] Umakanta, Choudhury, "Sensitivity Analysis in SPICE3", Master Report, University of California, Berkeley, December 1988.

[3-2] Soyeon Park, "Analysis and SPICE implementation of High Temperature Effects on MOSFET", Master's thesis, University of California, Berkeley, December 1986.

[3-3] Clement Szeto, "Simulator of Temperature Effects in MOSFETs (STEIM)", Master's thesis, University of California, Berkeley, May 1988.

Mixed-Mode Simulation

Mixed-Mode Simulation Overview

Modern circuits often contain a mixture of analog and digital circuits. To simulate these circuits efficiently, a combination of analog and digital simulation techniques is required. IsSpice4 supports three ways to model mixed-mode circuits.

- Exact transistor representations
- Boolean Logic Expressions
- Digital Primitives using an Embedded Logic Simulator

Exact representations are used in the analysis of analog circuits such as an IC where a close inspection of its I/O characteristics is needed, or for signal integrity problems where accurate waveforms are desired. They are created using subcircuit macro models. Boolean logic expressions are delayless functions that are used to provide efficient logic signal processing in an analog environment. They are created using the B element. These two modeling techniques use analog algorithms to provide the solution. The third method involves the use of digital primitive elements and the native event-driven simulation algorithm that is built into IsSpice4.

Digital circuit simulation differs from analog circuit simulation in several respects, but the primary difference is that a solution of Kirchoff's laws is not required. Instead, the simulator only determines whether a change in the logic state of a node has occurred and then propagates this change to connected

elements. Such a change is called an “event”. When an event occurs, the simulator examines only those circuit elements that are affected by the event. By comparison, analog simulators iteratively solve for the behavior of the entire circuit because of the forward and reverse transmission properties of analog components. This difference results in a considerable computational advantage for digital circuit simulators, which is reflected in the significantly greater speed of digital simulations. Therefore, it is vastly more efficient to simulate the digital portions of a design with a digital simulator, and the analog sections with SPICE. Only in cases where the two are inextricably dependent should a mixed approach be undertaken.

Two basic methods of implementing mixed-mode simulation are the “native mode” and “glued mode” approaches. Native mode simulators implement both analog and digital algorithms in the same executable, and use one input netlist. Unlike SPICE 3, which is designed mainly for analog simulation and is based exclusively on matrix solution techniques, IsSpice4 includes BOTH analog and event-driven simulation capabilities in the same executable. Thus, designs that contain significant portions of digital circuitry can be efficiently simulated together with the analog components.

The event-driven algorithm in IsSpice4 is general purpose and supports non-digital types of data. For example, elements can use real or integer values. Because the event-driven algorithm is faster than the standard SPICE matrix solution algorithm, reduced simulation time for circuits that include these elements occurs, as compared to a simulation of the same circuit using only analog models.

Glued mode simulators actually link two separate simulators, one analog and the other digital. This type of simulator must define an input/output protocol so that the two executables can communicate with each other effectively. The communication constraints tend to reduce the speed, and sometimes the accuracy of the complete simulator. On the other hand, the glued approach allows the component models for the separate executables to be used without modification.

Native Digital Simulation

The following 4 sections describe the event-driven simulator with relation to digital code models. Hence, it is sometimes referred to as a digital simulator even though the same algorithm processes all types of event-driven nodes. Most of the discussions center around how digital simulation is performed and digital values are processed. With the exception of how digital states are characterized, the information also applies to other user-defined node types such as real or integer.

States, Logic Levels and Strengths

The logic simulator in IsSpice4 is a 12-state digital simulator. A state refers to the value of a digital node. A state is characterized by a logic level and a strength. IsSpice4's digital simulator contains 3 logic levels and 4 strengths. Hence, the digital simulator is referred to as a 12-state simulator.

Logic Levels
There are three logic levels used to describe the state of a digital node. They are:

0	Low
1	High
U	Unknown

These logic levels do not correspond to any particular voltage. A Low has no analog voltage representation within the digital simulation. Special bridges, discussed in subsequent sections, are used to translate between analog voltages and logic levels.

Strengths
There are four strengths that are used to further describe the state of a digital node. They are:

s	STRONG
r	RESISTIVE
z	HI_IMPEDANC
u	UNDETERMINE

Each of these strengths represents an output classification of a digital element. A STRONG strength represents the output , which is expected from a standard bistate totem pole output. A HI_IMPEDANCE strength represents the output from an open collector device or a disabled tristate device. An UNDETERMINED strength represents an output that is generated by an unknown enable input for tristate devices. A RESISTIVE strength falls between the strength of a Strong, Low impedance, and a High impedance, disabled output. This strength would be equivalent to the on state of an open collector, pulled up to a high state.

When you combine the logic level with the strength, you obtain a value, referred to as the state, for a digital node. The digital simulator uses the states of all nodes attached to an input to determine the final controlling state of the input.

Digital values are specified, for digital input sources or state machines, as the logic level followed by the strength. Hence, you will use 0s to represent a Strong logic 0, or 1z to represent a high disabled tristate condition.

Events and Event Scheduling

An event is defined as any change in the state of a digital node. Input to a digital circuit is typically a list of desired logic states for particular digital nodes and the time in which these states are to occur. This event list is called an event schedule. As the digital simulation is performed, one or more of the scheduled events will produce other events that will be added to the schedule. The event-driven portion of the simulation stops when all events have been processed.

For purely digital circuits, the digital source produces the set of events that are to be scheduled. Additional events are scheduled depending on the activity of the circuit.

For mixed-mode simulations, events are scheduled by any combination of digital sources and/or analog signals fed to the

digital circuitry through the use of a special device called an Analog-to-Digital node bridge (A-to-D). Briefly, this device generates a logic level output with a STRONG strength, which depends on the input signal and the bridge's model definition. The state and the time in which it was generated are passed to the digital simulator and scheduled as an event.

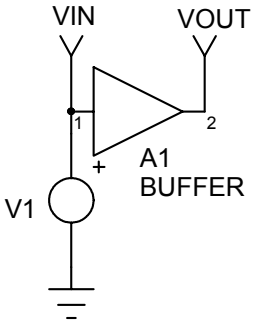
Gate Delays

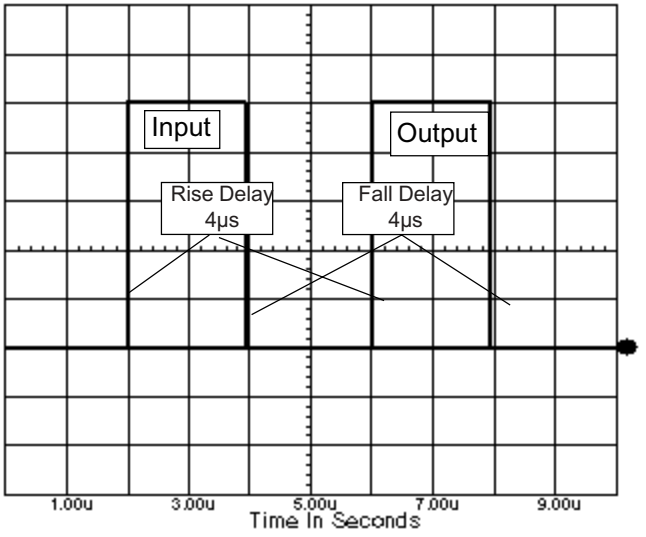
IsSpice4 uses an ideal delay model, which is also known as the transmission line, or group delay model. This type of model propagates the input directly to the output, delayed by the time specified in the element's model statement. Most digital models allow separate rise and fall delays.

As an example, the output of a simple buffer circuit is shown. The rise delay and fall delay were both specified as 4µs.

The delay of an output event from an input event is formed by adding the device's delay to the start of the input event. The resulting event is an exact representation of the input event delayed by the time specified in the device's model statement.

A buffer containing a 4µs rise and fall delay.



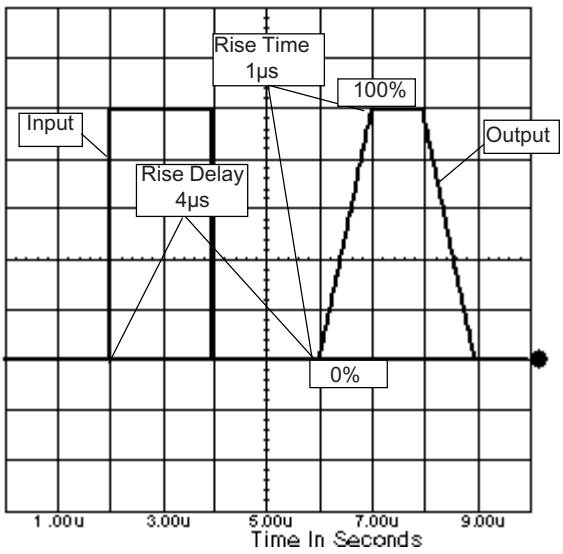


When interfacing analog signals, delays can be accumulated through the A-to-D interface model. In this case, a rise delay is accumulated from the time the analog input signal reaches the in_low model parameter. A fall delay is accumulated from the time the analog signal reaches the in_high model parameter.

Rise and Fall Times

Rise and fall times are specified as 0% to 100% values, not 10% to 90% values.

Rise and fall times are analog artifacts of digital circuits. As such, they are not included in the digital simulator or in any of the digital models. All rise and fall times are added during the Digital-to-Analog conversion made by the (D-to-A) node bridges. All rise and fall times are implemented as linear transitions from the defined high to low voltage, and do not represent the 10%-90% slope, but rather the 0%-100% slope. Rise and fall times are added after all delays have been accumulated.



Node Types and Translation

Before you develop a mixed-mode circuit, it is important to understand how analog and event-driven models are connected. Every element has one or more input and/or output ports. Each port is characterized by a node type. IsSpice4 contains two basic node types; analog, which connects to the SPICE 3 simulation kernel, and event-driven, which connects to the discrete event-driven simulator. Event-driven, nodes can be subdivided into digital, real, integer, and user-defined types.

Real node types use double-precision floating point data. They are useful for evaluating sampled-data filters and systems. Integer node types use integer data. They are useful for evaluating round-off error effects in sampled-data systems. The Intusoft Code Modeling Kit allows you to define alternate node types that operate with the event-driven algorithm. These "User-Defined Nodes" allow code models to pass arbitrary data structures without having to worry about conversion to a predefined node type. IsSpice4's digital simulation is actually implemented as a special case of this User-Defined Node capability, where the digital state is defined by a data structure that holds a Boolean logic state and a strength value.

All IsSpice4 elements are classified by their node types. Hence, all traditional SPICE 3 elements are classified as analog because they have analog node types. Code models may be analog, event-driven, or both (a hybrid) depending on their node types. For example, digital code models have only digital inputs and outputs.

In order to connect elements with different node types, a translational element known as a bridge must be used. The schematic will insert the correct bridge if the model or subcircuit entry in the library contains the *FAMILY syntax extension. See the SpiceNet help on "Library Structure" for more information.

For example, to connect an analog element to a digital element, you must use an analog to digital (A-to-D) node bridge.

Analog and Digital Interfaces

Node bridges are inserted by the schematic for digital parts taken from the ICAP/4 libraries.

When analog elements are mixed with digital elements, special connections between the two must be made. These connections must be capable of translating continuous time analog signals to and from discrete digital states. Special components called Analog-to-Digital (A-to-D) and Digital-to-Analog (D-to-A) **Node Bridges** are used for this task. These node bridges are the key to effective mixed-mode simulation.

Translating Analog to Digital (A-to-D)
The Analog-to-digital (A-to-D) bridge is used to translate a continuous time analog signal into a discrete digital event. The A-to-D produces a STRONG digital event with a logic level determined by the input signal and the in_low and in_high model parameters. If the input analog signal falls between in_low and in_high, an undefined state is generated. These values are analogous to the VIH and VIL parameters used to describe the input of TTL gates. The delays, rise_delay and fall_delay, associated with this model, are accumulated after the voltages, in_low or in_high respectively, have been reached.

The input to the A-to-D is a high impedance path and does not load the circuit. The input can be any voltage or current.

Translating Digital to Analog (D-to-A)
The Digital-to-Analog (D-to-A) bridge is used to translate a discrete digital event into a continuous analog signal. The D-to-A outputs an analog value of out_low for a logic 0 input, and out_high for a logic 1 input. The output change has a t_rise, or t_fall, implemented as a linear transition. Any undetermined input generates an analog output voltage equal to the out_undef parameter. The output of a digital gate is essentially a voltage source with infinite driving capabilities.

Note: The arrow in the A2D and D2A schematic symbols indicates the signal direction. For example, for the A2D the input signal must be analog. An error will result if you try to connect the digital side of the A2D to a digital output.

Mixing Digital and Analog Circuitry

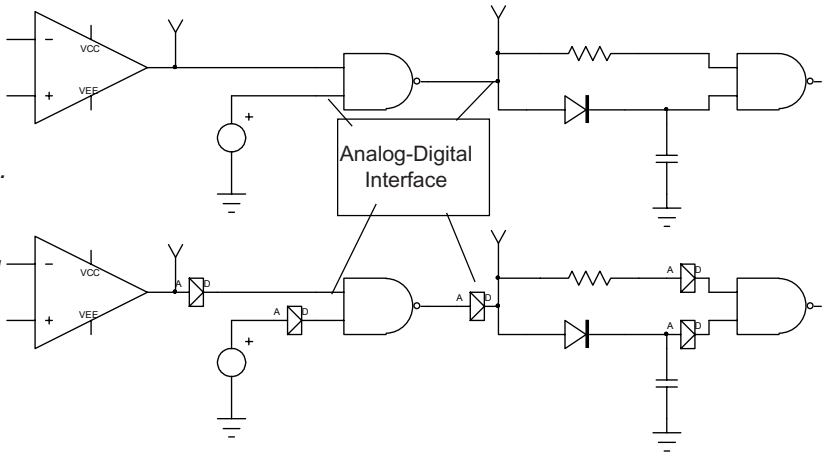
In order to speed a mixed-mode simulation, every attempt should be made to minimize the use of A-to-D and D-to-A elements. Large groups of digital elements should be connected together directly. The interface change between analog and digital circuitry should only be made when absolutely necessary.

Node Bridges must be used when connecting any analog node to any kind of event-driven node.

Each D-to-A element will introduce a set of break points around the minimum and maximum voltage in order to provide a smooth transition and to aid convergence. Inserting excessive D-to-As will add excessive numbers of breakpoints, increasing memory use and decreasing simulation speed. A similar problem arises when A-to-Ds are used excessively. In order to ensure that an event is triggered accurately, the values at the inputs of A-to-Ds are checked at every recorded time point. It is easy to see that if numerous A-to-Ds are used, the simulation will spend a great deal of time checking to see if an event should be generated.

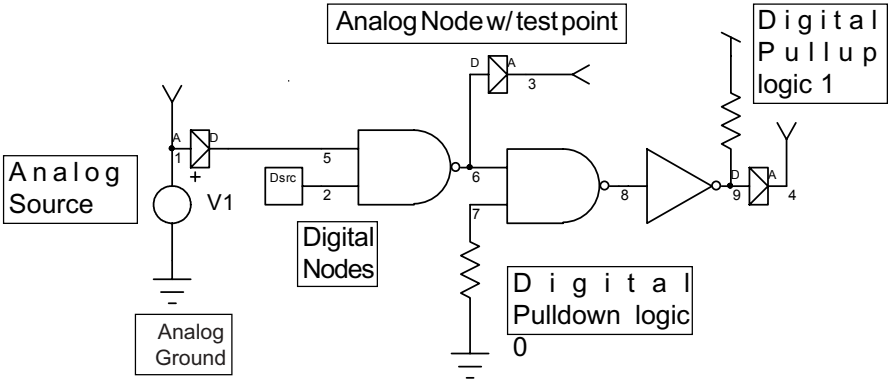
As an example, the circuit on top shows a hypothetical set of connections. The circuit on the bottom shows how the circuit would actually be drawn in a schematic. Note the use of bridges at each analog-digital interface.

The arrow in the A2D and D2A symbols indicates the signal direction. You can't use an A2D as a D2A by flipping it!!!



Viewing Digital Data

For digital nodes, the SpiceNet schematic will automatically insert a D-to-A node bridge if you put a test point on a digital node. If you are working from a netlist you will have to insert the bridges manually. The following schematic shows where the schematic would insert node bridges. Note that even though the bridges are inserted, the will not be shown on the schematic. They will however, be represented in the IsSpice4 netlist.



Once the D2A symbol is connected to the digital node, a normal test point symbol, or IsSpice4 .PRINT statement can be added. No load is required on the output of the D-to-A.

Creating Digital Stimulus

You can not use independent or dependent voltage or current sources to drive digital circuits. This is because you can not connect an analog node directly to a digital node. There are several ways to create digital stimulus.

1) Use the Digital Source or Digital Oscillator (DVCO) code models. The digital source requires an external text file describing the stimulus (See the Code Model Syntax chapter). The digital source can produce data for any number of bits.

2) Use any analog type of stimulus, or signal. SpiceNet will automatically connect an A-to-D node bridge between the source and the digital circuitry.

3) Use the Pullup and Pulldown code models for logic 1 and logic 0 stimulus.

Referring to the schematic in the previous section, notice how the analog source and A-to-D are used to drive the nand gate on the left. The DSRC symbol represents a single bit digital source. Other predefined symbols are available and other bit configurations can easily be created. Notice the pullup and pulldown symbols. They can be used whenever a steady logic 1 or 0 stimulus is required.

Reducing Circuit Complexity

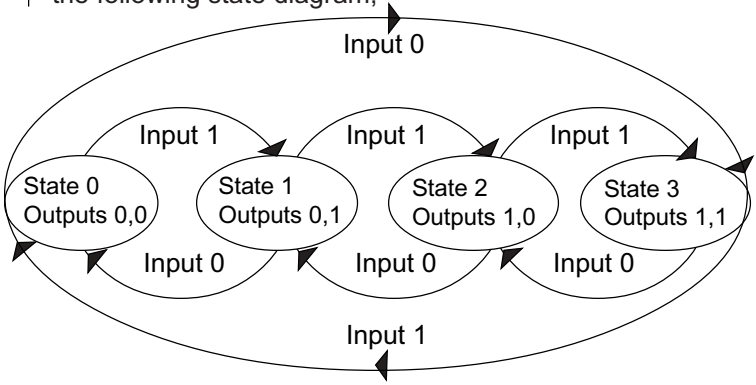
One method of increasing the efficiency of the simulation is to take advantage of the state machine element. This code model can be used to replace large sections of clocked combinational circuitry, such as a counter, with an equivalent, but much faster, representation. For instance, a 4 state up-down counter, as shown, can be simulated with a single state machine model, essentially replacing the flip-flops and control gates that would normally be required.

The state machine code model can be easily configured to represent a wide variety of clocked combinational digital circuitry.

The state machine code model is configured by an initialization (text) file that is read when the circuit file is loaded by IsSpice4. The file should be stored in your working directory. The format for the file is given as;

Present State Outputs Inputs Destination State

Thus in order to describe the up-down counter represented by the following state diagram;



See the State Machine in the Code Model Syntax chapter.

The state initialization file would look something like;

*Present State	Outputs @this State		Input(s)		Destination
0	0s	0s	0	->	3
			1	->	1
1	0s	1z	0	->	0
			1	->	2
2	1z	0s	0	->	1
			1	->	3
3	1z	1z	0	->	2
			1	->	0

Strengths
s=strong
u=undetermined
r=resistive
z=hi_impedance

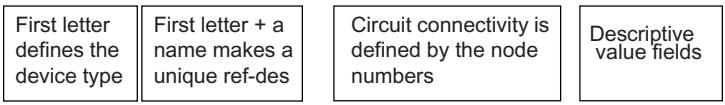
The output levels that are to be assumed by the state machine are defined by the logic level and output strength. In this case, the outputs are 0s, representing a STRONG low digital signal, and 1z, representing a high enabled tristate digital signal. All of the available logic levels and strengths are discussed in the States, Logic Levels and Strengths section at the beginning of this chapter.

Netlist Definition

IsSpice4 Netlist

A circuit is described to IsSpice4 by a netlist. A netlist is a standard text file that contains several types of statements that describe the circuit and tell the simulator what to do. These statements fall under the following categories: Element Descriptions, Analysis Control, Device Modeling, Output Control, ICL functions, Simulation Templates, and Miscellaneous statements used for netlist construction.

Element description statements contain the device type, nodal connectivity, and parameter values. A typical element description statement for a resistor is:

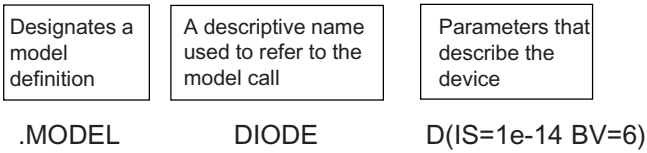


Valid reference designations include: R1, QName, and M3n01.

Analysis control statements determine what type of analysis the simulator will perform and how the data will be collected. There is also access to a variety of internal program defaults through the .OPTIONS and ICL Set statements. A typical control statement to run a transient analysis is:

```
.tran    1u    200u
```

In addition to the parameters on the Element Description line, device modeling statements are required to further describe some elements. A typical .Model statement for a diode is:

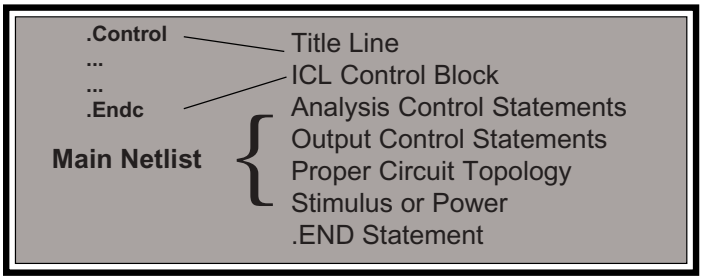


Output Control is specified through the use of .PRINT, .PLOT, and .VIEW statements. Most, but not all analysis control statements require one of these statements to generate results. Output can also be generated using the ICL Save, Print, View, Show, and Showmod commands.

Netlist Structure

Text may be in upper or lower case.

The statements in the main part of the IsSpice4 netlist can be in any order. However, the statements in the ICL control block are order dependent. There are six essential statements that must be present in order to perform a simulation:



The Title and .END lines

The first line must be a title line.

All netlists must have a title line and a .END line. The title is the first line in the netlist. Any circuit information on this line will be ignored by IsSpice4.

The .END statement must be the last line in the netlist. This marks the end of the circuit description.

ICL Statements and Control Block

The ICL block must be at the top of the netlist before IsSpice4 "dot" control statements and after the title.

ICL stands for Interactive Command Language. It is an extension of the basic set of functions that run SPICE language and provides expanded printing/data output capabilities, Simulation Breakpoints, and multiple analysis loops. ICL statements can be entered directly in IsSpice4's simulation control dialog's Script window or run batch-style from the input netlist. The IntuScope5 waveform analyzer also uses ICL commands. If the IsSpice4 Script window is used, the ICL statements can be run interactively. This allows easy script debugging. The ICL section of the netlist begins with a ".control" line and ends with a ".endc" line. Standard IsSpice4 "dot" control statements should be placed after the ICL block. ICL statements can also be issued one at a time in the netlist, without the .control and .endc wrappers, simply by placing "*#" before the command. The usage of ICL functions is explained in Chapter 11. The syntax reference guide for all ICL functions can be found in the on-line help.

Analysis Control Statements

Analysis control statements can be included in the ICL control block or the Simulation Control dialog.

The group of statements used to specify what type of analyses will be performed are called “control statements”. These statements begin with a dot, “.”, followed by a control statement directive.

For Example:

.AC DEC 10 1HZ 1MEGHZ	Run an AC Analysis
.TRAN .1US 10US	Run a Transient Analysis
.OPTIONS RELTOL=.01	Change Default Options

Note: The statements required to run a particular analysis will vary. For a transfer function, only the .TF statement is needed. For a DC analysis, only the .DC and .PRINT DC statements are needed. However, for some analysis types, such as the AC or distortion analysis, an independent source with the proper stimulus, along with a control statement for the analysis type and a control statement to collect data, must all be present for the analysis to run properly. For example, to run an AC analysis, there must be a .AC statement and a .PRINT AC statement, as well as the AC keyword on at least one independent source.

Output Control Statements

Output for analog nodes is obtained by including one or more of the following control statements in the netlist: .PRINT, .PLOT or .VIEW. ICL commands can also be used to create output. Digital and other types of event driven nodes must be translated to analog nodes before output can be generated. For more information, please refer to the Viewing Digital Output section in the Mixed-Mode Simulation chapter.

PRINT and PLOT

The .PRINT and .PLOT statements are used to generate scalar and vector data in the output file. Data for the following quantities can be saved: node voltages, device currents, computed device parameters, and math expressions containing aforementioned quantities. Most major analysis types (AC, DC,

The @notation is used to reference computed device parameters listed in the IsSpice4 on-line help. #:XName is the syntax used to reference subcircuits.

TRAN) require at least one print or plot statement to appear in the netlist. Typical .PRINT statements are:

Designates tabular output data	Specifies that the output is for a DC or transient analysis	Voltages, currents, and device parameters can be recorded

```
.PRINT      DC      V(1)  I(V1)
.PRINT      TRAN    @M1[gm] V(12:XSUB)
```

Node voltages are recorded with respect to ground unless a voltage difference is specified. Therefore, specifying V(3,0) is invalid. A voltage difference is specified by including two nodes separated by a comma within parentheses. For example, .print tran V(3,4) will generate the voltage difference between nodes 3 and 4.

VIEW

The .VIEW statement overrides the default scaling values set by the .OPTIONS VSCALE, ISCALE, and LOGSCALE parameters.

The .VIEW control statement is used to scale a waveform that is shown in the real-time simulation display. One or more of these statements can appear in the netlist. Only one vector is scaled by each statement. A typical .VIEW statement for a transient analysis is:

Designates graphical output	Specifies that the output is for a transient analysis	Specifies which node to scale	Specifies lower and upper scaling

```
.VIEW       TRAN        V(1)        -1    1
```

Measuring Current

Current can be measured through any device and for semiconductor junctions. **Voltage sources are not required** as in SPICE 2 programs. Subcircuit currents can also be measured.

Example: Measuring Semiconductor Currents

```
.PRINT TRAN @q2[ie] @m1[id]
```

Example: Device Currents

```
.PRINT TRAN  @r1[i] @Lcore[i]
```

The above examples measure the BJT emitter, MOSFET drain, resistor, and inductor currents.

Print Expressions
Mathematical combinations of any set of PRINT vectors can be saved in the output file. A variety of built-in math functions are also available. Please refer to the ICL let and alias commands discussed in Chapter 11 for more information.

Circuit Topology Definition

Digital and other types of code models have special netlist requirements. Please refer to the Using Code Models section in this chapter.

The topology of a circuit is defined by Device Description statements. These statements will define a device type, its nodal connections and any parameters necessary to describe the device. Digital models, and other code models, have special netlist requirements. See the Using Code Models section.

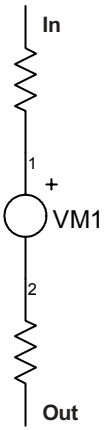
Device Types
The type of device, either passive, active, code model, or subcircuit, is specified by the first letter of the name given in the Device Description statement. This is also referred to as the reference designation, or ref-des.

IsSpice4 allows ref-des names with more than 8 characters.

Device	Definition
Rload 1 2 100	defines a 100Ω resistor
Qin1 2 4 5 Spnp	calls a transistor named Spnp
VIN 10 0 5V	defines a 5 volt voltage source
A1 22 25 s_001	calls the code model s_001
Xcomp 2 3 5 6 10 11 LM311	calls a subcircuit named LM311

In the above examples, the first letter of the ref-des in each line is used to define the type of device. The rest of the ref-des is used to make the element description unique. Any alphanumeric string can be placed after the first letter. You can not use duplicate reference designations.

Node Connections
All connections between devices are determined by node numbers, or node names, given on the Device Description statement. Nodes can be defined by any alphanumeric string. However, positive integers are usually used for clarity. For example, the voltage source on the next page is defined by:



VM1 1 2

where V defines a voltage source, VM1 is the unique ref-des name, and the source is connected between nodes 1 and 2.

A connection is made by assigning the same node number or node name to the devices you want to connect. For example, the circuit to the left would generate the following lines:

```
VM1 1  2
R1  1  In  100k
L1  2  Out  10u
```

Notice the use of the node names In and Out to describe the top connection of the resistor and the bottom connection of the inductor.

A component must have a connection for each input or output terminal defined for the device. By definition, a resistor has two terminals. Hence, a node must be assigned to each of these terminals.

Exceptions for Node Names

To avoid any conflicts, names should be restricted to alphanumeric characters. Characters and names that are used in IsSpice4 statements, such as "+, /, ?, |, -, ~, &, sin, abs, TIME, FREQ, TEMP, SET, TRAN, STOP, or SHOW, etc. should not be used for node names. It is recommended that SPICE 2 style limitations such as names beginning with a letter instead of a number, are maintained. For example, it would be better to call a node "A1" rather than "1A" so that the 1A could not be accidently confused with a value of one Ampere.

When generating output for a node voltage, it is important to note that a node name must appear on the .PRINT line without parentheses or the V voltage designator. This is different from a node number specification. The example below generates voltages for the node number 33 and the node name "output":

Correct	**Incorrect**
.PRINT TRAN output V(33)	.PRINT TRAN V(output) V(33)

Node names are used differently in the .PRINT statement than in other control statements.

For the B dependent source, or in any control statement other than the .PRINT statement, node names are referenced the same as node numbers. For example, V(node_name).

Correct	**Incorrect**
B1 1 2 V = V(output)	B1 1 2 V = output

Ground

Ground, node 0, is only used for analog devices. For a logic 0 (digital ground), digital devices should use the pulldown code model.

Node 0 is reserved by IsSpice4 to represent ground, whether it is in the main circuit or in a subcircuit. Every circuit must have at least one connection to ground. Note: Unlike SPICE 2, IsSpice4 does not require a DC path to ground for every node, although this is generally a good rule of thumb.

Component Values and Model Names

After declaring the proper device type and node connections, the final step is to give the device an appropriate value or values. Most devices require at least one parameter. For example, a definition for a resistor would be:

RF 23 1 100k

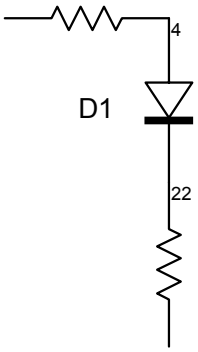
where the resistor RF is connected between nodes 23 and 1 and has a value of 100kΩ.

Numerical entries can use an integer format, floating point 'E' format, and be scaled by attaching one of the following entries:

T 1E12	**MIL 25.4E-6**
G 1E9	**U 1E-6**
MEG ... 1E6	**N 1E-9**
K 1E3	**P 1E-12**
M 1E-3	**F 1E-15**

Units following the scaling parameter are ignored as long as they are connected to the value and not separated by any field delimiters (spaces, commas, etc.). For example, the numbers 1000, 1000.0, 1K, 1KV, 1KOHM, and 1E3 are all equivalent numerical representations.

Negative values are allowed.



Note: Resistors, capacitors, and inductors can accept negative values.

Certain devices require a model name as a parameter. Model names can be upper or lower case. Any additional parameters can be added on the line separated by delimiters. The example to the left would be defined by;

D1 4 22 DIODE

The line describes a diode, D1, connected between nodes 4 and 22, calling a model named “DIODE”. To make this call to a diode complete, there must be a .MODEL statement somewhere in the netlist to define the model “DIODE”.

Note: Unlike in SPICE 2, model names can have more than eight characters and begin with a number. However, for backward compatibility with SPICE 2, this feature shouldn’t be used.

MODEL Statements

All code models, including digital elements, require a .Model statement.

The .MODEL statement contains a list of parameters that define a device’s behavior. The parameters are inserted into equations, which are evaluated during each analysis. A .MODEL statement consists of the .MODEL keyword, followed by a field containing a unique model name, a keyword describing the type of model, and the parameters used to describe the device. An example would be:

Designates a model statement	Name given to identify the model	Specifies a diode model type	List of diode parameters
.MODEL	DN4148	D	(IS=8E-13 BV=6)

Here, the model name is “DN4148”. The “D” entry shows that the model statement describes a diode. And finally, the parameters IS and BV describe the diode’s behavior. The

parameter list will vary, but any parameters aren't listed will be set to their default values. The .MODEL statement must be called by a diode Device Description line, for example:

D1 2 34 DN4148

Multiple diodes may refer to a single model statement.

Model Information In Subcircuits
In order to refer to input and computed model parameters inside subcircuits, IsSpice4 uses the following syntax:

Model Parameters - ref-des_name:Xname1:Xname2:... : [Param_name]

where Xname1 and Xname2 are the names, including the letter X on the subcircuit call line, and ref-des is the name including the keyletter on the device call line. For example, to output the model parameters from the model called by J1, we would use the following:

The Showmod function is described in Chapter 11.

```
.control          ; Beginning of ICL control block
op
showmod J1:X1     ; Displays the model parameters for the
.endc             ; JFET J1 in subcircuit X1
```

Subcircuit Netlist

A subcircuit is a set of components that describe a subsystem or component that can not be defined with a single device description line. Subcircuits are constructed by encompassing a netlist that describes the circuit with a .SUBCKT statement at the beginning, and a .ENDS statement at the end. The .SUBCKT line contains the name of the subcircuit and the node numbers that connect to the input and output points in the subcircuit. The format is:

.SUBCKT [name] [nodes]

The .ENDS statement marks the end of a subcircuit description.

For example, the following describes an RC subcircuit;

```
.SUBCKT RC 1 2
R1 1 2 100K
C1 2 0 10P
.ENDS
```

The components R1 and C1 define the subcircuit. The subcircuit has two external connections at nodes 1 and 2. Notice that node 0 is used inside the subcircuit. This node 0 and node 0 in the main circuit both represent ground. This subcircuit would be called in the main circuit netlist by the statement;

```
XRC 22 44 RC
```

where nodes 22 and 44 in the main circuit would connect to nodes 1 and 2 in the subcircuit.

Node and Device Information In Subcircuits

In order to refer to nodes and computed device parameters inside subcircuits, IsSpice4 uses the following syntax:

Node Voltages - V(node:Xname1:Xname2:...)
Device Parameters - ref-des_name:Xname1:Xname2:...[Param_name]

where Xname1 and Xname2 are the names, including the letter X on the subcircuit call line, ref-des is the name including the keyletter, and Param_name is the name of an input or output device parameter (See Appendix B). For example, to print the subcircuit voltage at node 2 and the current in resistor R1, we would use the following:

See the on-line help for more information on Device parameters.

```
XSUB  In Out  TEST        ; Call to subcircuit

.SUBCKT TEST 1 3
R1 1 2 1K
L2 2 3 1UH
C3 3 0 1P
.ENDS

.PRINT TRAN V(2:XSUB) @R1:XSUB[i]    ; Print statement
```

Miscellaneous Netlist Statements

Comment
Comment lines are ignored by the IsSpice4 simulator. Any line beginning with an asterisk, "*", is considered a comment line. Any text at the end of a line that is preceded by a semicolon is considered an in-line comment. Comment lines can be inserted anywhere in the netlist, and have absolutely no effect on the simulation.

For Example:
```
* This is a comment line
R1 1 0 10   ; This is an in-line comment
```

There is no specific limit to the number of continuation lines that can be used in IsSpice4.

Continuation line
In certain circumstances, in may be necessary to use more than one line to describe a statement. A plus sign, "+" in the first column is used to signify a continuation line. Any line with a "+" in the first column will be interpreted as part of the preceding line. There is no limit to the number of continuation lines.

For Example:
```
Vin 1 0 pwl 0 1 10u -1 20u 1 30u -1 40u 1 50u -1
+ 60 1 70u -1 80u 1 90u -1 100u 1 110u 0
```

Delimiters and the Comma

Spaces, new lines, the equal sign, comma, a right parentheses or a left parentheses are all evaluated as delimiters and are used to separate various fields in a netlist.

A special exception is made for the comma. A comma is evaluated as a comma when it is inside a set of parentheses. It is used as a delimiter everywhere else. For example, ".PRINT TRAN V(1,2)" will evaluate the comma as a comma and record the difference between the voltages. The statement ".PRINT TRAN V(1),V(2)" will evaluate the comma as a delimiter and produce the voltage at node 1 and the voltage at node 2.

IsSpice4 Netlist Construction

Now that the format of the different lines has been briefly discussed, it is time to discuss the construction of the netlist itself. As stated earlier, IsSpice4 can appear in any order except for the title, the ICL control block, and the .END statement. These three items are position-dependent. A typical netlist is shown below.

Title

ICL Control Block

Simulator and Output Control

Circuit Description

Models

.END

```
SAMPLE CIRCUIT
.control
save all
op
show  q1 q2
.endc
.AC  DEC  10  1  1G
.TRAN   1N   100N
.OPTIONS   ACCT
.PRINT AC   I(V3)   IP(V3)
.PRINT TRAN  V(4)   I(V3)   V(7)   V(8)
V1  1  0  AC  1  PULSE  0  1  0  0  0  50N
C1  1  2  .01U
R1  2  7  390
Q1  3  7  0  QN2222
Q2  11  3  5  QN2222
Q3  8  5  4  QN2222
R2  7  5  390
R3  4  0  50
R4  5  0  390
V2  6  0  -2
R5  6  7  820
V3  9  8
D1 11 9 DLASER
R6 11 3 750
V4 11 0  5
.MODEL QN2222 NPN(IS=1.9E-14 BF=150 VAF=100
+ IKF=.175 ISE=5E-11 NE=2.5 BR=7.5 VAR=6.38
+ IKR=.012 ISC=1.9E-13  NC=1.2 RC=.4 XTB=1.5
+ CJE=26PF TF=.5E-9 CJC=11PF TR=30E-9
+ KF=3.2E-16 AF=1.0)
.MODEL DLASER D N=2
.END
```

IsSpice4 Output Files

The output file from IsSpice4 is compatible with output files generated by Berkeley SPICE version 2. Data is stored in the same tabular and printer-plot formats. For major analysis types, the only differences are in the structure of the analysis banners and the addition of an index column for tabular .PRINT data.

IsSpice4 output files have the same name as the input file, but the file extension ".out" replaces the input file extension ".cir".

An additional feature of IsSpice4 is that a complete netlist, with all subcircuits flattened, can be saved in the output file if the .OPTIONS parameter LIST is inserted. This can be quite useful for troubleshooting subcircuits. The flattened netlist format is:

device ref des : Xname1 : Xname2 : ...

For example:

```
rp:x1 7 9 10k
rxx:x1 7 0 10meg
rp:x2 7 9 10k
rxx:x2 7 0 10meg
```

The first line refers to the resistor "rp" in the subcircuit that is called by X1. The last entry refers to the resistor "rxx" in the subcircuit called by X2.

In addition, node voltages for subcircuit nodes will also use this extended syntax. For example:

```
 V(10:x1)      -2.16891e-08
 V(11:x1)      -2.16891e-08
....
 V(10:x2)      2.745771e-03
 V(11:x2)      -1.85348e-08
 V(12:x2)      -1.85348e-08
```

The first line refers to the node voltage of node 10 in subcircuit 1. The last line refers to the voltage at node 12 in subcircuit 2.

Note: Reference designators that only have the IsSpice4 keyletter but no name will have an underscore appended to the name. For example, the inductor in

```
.Subckt Test 1 2 3
L  1 2 10u
R1 2 3 1
.Ends
```

would be referred to as @L_. Hence, the flux for this element would be obtained by @L_:Xname...[flux].

Simulation Template Output
Output data produced Simulation Template based analyses (RSS, EVA, Worst Case, and Sensitivity) is placed in the output file. The output data format is controlled by the scripts in the template file. These may be modified using any text editor.

Tabular Output Data Index
The tabular output data produced by the .PRINT statement will include a column called Index. The Index column contains a number for each data point that is equal to the location in the vector. The index value is used by various ICL commands to access data within a print vector.

Error And Warning Messages
All error and warning messages encountered during the simulation will be placed in the Errors and Status Window. Since some of the errors can cause a simulation to abort, the error and warning messages are also placed in a separate file with the same name as the input file and the file extension ".ERR". For example, errors in SAMPLE.CIR are placed in a file called SAMPLE.ERR. This is different than SPICE 2, which placed error and warning messages somewhat randomly in the output file.

Important Note: If there are any problems with the simulation, the data appears to be in error, or if there is a flashing question mark symbol at the upper left corner of the IsSpice4 screen, you should check the .ERR file for messages.

Code Model Netlist Structure

IsSpice4 includes a special set of C code language based elements. These “code models” can be used like any standard SPICE primitive device (Diode, BJT, etc.). Code models, however, use a slightly different netlist syntax. All code model call lines begin with the letter “A” and require a companion .Model statement. Like SPICE semiconductors, more than one code model can use a previously defined .Model statement. The following example demonstrates the use of the limiter code model;

```
A1 1 2 limit1
.Model  limit1  limit(in_offset=.1 gain=2.5 out_lower_limit=-5
+ out_upper_limit=5 limit_range-.1 fraction=FALSE)
```

The expected node order for each code model call line can be found in the Port Table, which is given for each device in the Code Model Syntax chapter. The Port table describes the types of inputs that can be used to drive the device and the default input type. For example, the default input type for the limit code model is a voltage.

All the model parameters for each code model and their defaults, if any, are described in the Parameters Table and in the Code Model Syntax chapter.

Node Connections

Code models can have any combination of three different types of nodal connections; single-ended (ground referenced), differential, or vector. A single-ended node consists of a normal SPICE node designation. A differential node is specified by grouping two nodes in parentheses, such as;

```
a (1 2) 3 limit1
```

The parentheses indicate that the input to the element is a differential signal V(1)-V(2). Vector nodes are a bus type connection and are normally used on digital code models. For

Square braces, [ ], are used to enclose vector input nodes.

example, there is only one Nand code model, but it supports a vector type input. This allows the model to simulate any input configuration, for example, a 3-input Nand gate.

Anand [1 2 3] 4 nand3

Node 4 is a single-ended output.

Node Modifiers

The types of inputs that can be used for a particular code model are specified in the model's Port Table. The default port type entry specifies the type of input signal expected if no port modifier is present. To use an alternate type of input, one of the modifiers listed in the following Port Modifiers table can be inserted preceding the node number. Note: the alternate input must still be one of the types listed in the "allowed types" entry of the Port table.

Port Modifier Symbol	Interpretation
%v	represents a single-ended voltage port - one node name or number is expected for each port.
%i	represents a single-ended current port - one node name or number is expected for each port.
%g	represents a single-ended voltage-input, current-output (VCCS) port - one node name or number is expected for each port. This type of port is automatically an input/output.
%h	represents a single-ended current-input, voltage-output (CCVS) port - one node name or number is expected for each port. This type of port is automatically an input/output.
%d	represents a digital port - one node name or number is expected for each port. This type of port may be either an input or an output.
%vnam	represents the name of a voltage source, the current through the source is taken as the input.
%vd	represents a differential voltage port - two node names or numbers are expected for each port.
%id	represents a differential current port - two node names or numbers are expected for each port.
%gd	represents a differential VCCS port - two node names or numbers are expected for each port.
%hd	represents a differential CCVS port - two node names or numbers are expected for each port.

A port modifier symbol is not required if the default-type input signal is used, which is normally the case. Non-default port types (for multi-input or multi-output vector ports) must be specified by placing one of the symbols in front of each vector port. If all ports of a vector port are to be declared as having the same non-default type, then a symbol may be specified immediately prior to the opening bracket of the vector. The following examples should make this clear:

Example 1: - Specifies two differential voltage connections, one to nodes 1 & 2, and one to nodes 3 & 4.

```
%vd [1 2 3 4]
```

Example 2: - Specifies two single-ended connections to node 1 and node 2, and one differential connection to nodes 3 & 4.

```
%v [1 2 %vd 3 4]
```

Example 3: - Identical to the previous example except that parenthesis are added for additional clarity.

```
%v [1 2 %vd(3 4)]
```

Example 4: - Specifies that the node numbers are to be treated in the default type fashion for the particular model. If this model had “v” default-port type, then this notation would represent four single-ended voltage connections.

```
[1 2 3 4]
```

Example 5: - Normally the Table model uses a voltage input and a voltage output. Using the syntax below the table model would take an input voltage at node 1 and output the current between nodes 2 to 3.

```
A2 1 %id(2 3) Table
.Model Table pwl(xy_array=...)
```

Example 6: - Normally the limiter model uses a voltage input and a voltage output. Using the syntax below, the limiter model would take the current flowing through the source named VCC and output a differential voltage across nodes 2 to 3.

```
A2 %vnam(VCC) %vd(2 3) Limiter
   .Model Limiter limit(gain=...)
```

NULL Connections

The literal string "null", when included in a node list, is interpreted as no connection at that input to the model. "Null" is only allowed if the Null_Allowed value in the Port Table is "yes". "Null" is not allowed as the name of a model's input or output if the model only has one input or one output. Also, "null" should only be used to indicate a missing connection for a code model; use on other IsSPICE4 components is not interpreted as a missing connection, but will be interpreted as a node name. An example of the use of the null would be:

```
A1 1     2   NULL  NULL   3   4     DFF
*  data  clk nset  nreset  out nout
.MODEL DFF d_dff (...)
```

With the null key word added, connections to the nset and nreset pins of the D flip flop are not required. This feature is useful when setting up alternate configurations of code models in subcircuit macro models.

Inverting Digital Nodes

The tilde, "~", when added to a digital node name, specifies that the logical value of that node is inverted prior to being passed to the code model. This allows for simple inversion of input and output polarities of a digital model in order to handle logically equivalent cases and others that frequently arise in digital system design. The following example defines a NAND gate, one input of which is inverted:

```
A1 [~1 2] 3 Nand2
.Model Nand2 d_nand (rise_delay=1n...)
```

Extended Syntax

Introduction

By extending the normal SPICE syntax, several new capabilities have been added to the standard IsSpice4 capabilities. These include the ability to:

- Call models and subcircuits from library files
- Pass parameters to the main circuit and to subcircuits
- Define and substitute expressions for keywords
- Perform statistical yield analysis
- Sweep component and parameter values
- Optimize component and parameter values based on objective functions.

These syntax extensions are made compatible with IsSpice4 and other Berkeley compatible SPICE versions by processing the input netlist through a series of preprocessors. These preprocessors are; INCLUDE, DEFINE, PARAM, OPT and MONTE. The MONTE and OPT programs, which are used for defining component and parameter tolerances for performing a Monte Carlo analysis and for performing parameter sweeps and optimizations, will be covered in detail in a later chapter. Most of these syntax extensions are handled automatically by the ICAPS program and you do not need to be concerned with their individual operation; only the syntax extensions.

INCLUDE

The INCLUDE function searches stored model library files (ASCII) for all subcircuits and device models that are not already in your input netlist. The appropriate models and subcircuits are automatically appended to the IsSpice4 netlist, allowing you to perform circuit simulation without having to worry about entering complicated model statements or debugging subcircuit models and complex circuit hierarchies. Nested subcircuits and models are allowed. A simple open architecture library structure has been setup to facilitate maintenance and the addition of user-defined IsSpice4 models. INCLUDE can also be used to insert an entire file into your netlist.

DEFINE

The DEFINE function allows complicated expressions and statements to be defined by single keywords. These keywords can then be used throughout the netlist to decrease typing time and ease circuit debugging. Define statements may be placed anywhere in the netlist and will cause user-defined expressions to be substituted for keywords.

PARAM

The PARAM function is used to pass parameters into the main circuit and to subcircuits. They may then be used as-is or inserted into mathematical expressions. The mathematical expressions will then be evaluated using the passed parameters and replaced with a resultant value.

Error checking performed by these three preprocessors is only relative to the extended syntax. IsSpice4 will still error check the circuit topology and syntax.

Parameter Passing

There are several ways to model electronic components for use with the SPICE circuit simulation program. Each has several advantages and disadvantages. Intusoft has pioneered a number of different modeling techniques, enabling the SPICE user to have the maximum flexibility and power when modeling components. This section describes one of those modeling techniques, a technique called **Parameter Passing**.

Many electronic devices can be represented through the use of equations that are based on known or measured values. It would be helpful if these equations could be incorporated into a SPICE model and the model's behavior controlled by supplying the dependent variables. This is exactly what Parameter Passing accomplishes.

Parameters can be passed from a .PARAM statement to the main circuit or to subcircuits via the X subcircuit call line. Parameters can also be passed directly from a subcircuit call line (X line) into a subcircuit. In both cases, parameters passed into a subcircuit can be further passed to another subcircuit down the hierarchy. Parameters can be used alone or as part of an expression.

Example, Parameter Passing To The Main Circuit:

```
.PARAM T1=1U T2=5U
V1 1 0 Pulse 0 1 0 {T1} {2*T1} {T2} {3*T2}
```

After parameters are passed and evaluated

```
V1 1 0 Pulse 0 1 0 1U 2U 5U 15U
```

Example, Parameter Passing To Subcircuits:

```
X1 1 2 3 4 XFMR {RATIO=3}
```

Subcircuit syntax before evaluation

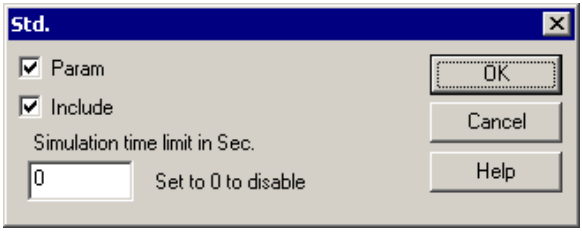
```
.SUBCKT XFMR 1 2 3 4
RP 1 2 1MEG
E1 5 4 1 2 {RATIO} ; parameterized expression in curly braces
F1 1 2 VM {RATIO * 2}
RS 6 3 1U
VM 5 6
.ENDS
```

Subcircuit after parameters are passed and evaluated

```
.SUBCKT XFMR 1 2 3 4
RP 1 2 1MEG
E1 5 4 1 2  3
F1 1 2 VM  6
RS 6 3 1U
VM 5 6
.ENDS
```

In the example, you can see that the subcircuit model for the transformer, XFMR, can represent many different transformers by merely changing the value of RATIO. Therefore, it is not necessary to construct a different subcircuit for every turns ratio. The turns ratio can be set at runtime and the PARAM function will take care of passing the parameter and generating calculating the correct values.

Parameter passing can be turned off by un-checking Param setting in Advanced Setup Options Dialogs. This option is available in Standard, Monte, Optimize, and Sweep Dialogs.



The Standard (Std.) Dialog contains two check boxes; one for Include (including models/subcircuits from libraries) and one for Param (Parameter Passing).

When checked, the Param function will run prior to any simulation passing any parameter lists to the subcircuits and constructing the proper netlist.

.PARAM Syntax

Do NOT reference any voltage or current in your parameter expression. Your parameter expression must be reducible to a single numeric value when evaluated.

Format: .PARAM *name1* = *value1* ... *namen* = *valuen*
.PARAM *name1* = { *expression1* } ...
+ *namen* = { *expressionn* }

Examples:
.PARAM VCC = 12V, VEE = -12V

.PARAM FRQ=10K, Period={1/FRQ}, TRISE = {period/100}
.PARAM PI = 3.14159, TWO_PI = {2 * 3.14159}
.PARAM TEST = 1, Phase = 90
.PARAM K1 = {10 * Sin(Test) / 1 + TEST/180}
.PARAM K2 = {TEST < 1 ? PI : Exp(Test^2) * 5K}
.PARAM K3 = {min(K1,1)}

PARAM Expressions

Expression	Evaluates to
{TEST}	1 with TEST = 1
{TEST/100}	.001 with TEST = 1
{TEST + 1K * TEST}	1001 with TEST = 1
{TEST > 0 ? 1K : 0}	1k with TEST greater than 0, else = 0

B element expressions and analog behavioral functions are detailed in Chapter 8.

The .PARAM statement defines the value of a parameter. A parameter name can be used in place of most numeric values in the circuit description or passed into a subcircuit. Parameters can be constants, or expressions involving other parameters. Param expressions may also take on the same form and features of analog behavioral element expressions including In-Line Equations, If-Then-Else statements, and analog behavioral functions.

Name cannot begin with a number. The parameter values must be either constants or expressions. Curly braces are optional for constants or single parameters, but mandatory for all expressions. *Expression* can contain constants, parameters, or mathematical operators similar to the B element. The .PARAM statements are order independent but parameter values must be completely defined such that all expressions can be evaluated to a resultant numeric value. A .PARAM statement can be used inside a subcircuit definition to establish local subcircuit parameters.

Parameters can be values or expressions. Parameter evaluation is not order dependent. However, all values must be defined for all expressions. Parameters and parameterized equations can be used in just about any facet of the design including but not limited to: all numeric element properties (including transmission lines and polynomials), analysis statements (.AC, Tran, ICL), and independent sources (PWL, etc.).

Note: The IsSpice4 parameter passing syntax is compatible with the PSpice PARAMS:, .PARAM, and parameterized expression syntax.

PARAM Rules and Limitations

The PARAM function evaluates expressions in the main circuit or in subcircuits using .PARAM statement variables, passed parameters or default parameters. Expressions may be as complex or as simple as desired. Several rules follow;

- Parameters defined in the main circuit file are applied to all subcircuits. Parameters defined in a subcircuit apply only within the subcircuit definition. Passed parameters override all other parameters of the same name.

- Parameters on the X subcircuit call line override parameter defaults on the .SUBCKT line. .SUBCKT line parameters override .PARAM values. .PARAM values override if no X line or .SUBCKT line parameters exist.

- The standard evaluation hierarchy is used, that is, items in parentheses are evaluated first, followed by ^, /, *, -, and +. The resulting value is inserted using engineering notation with 5 digit precision; for example, 1.3257MEG.

- Unlike IsSpice4, spaces are ignored. They are not used as delimiters within an expression.

- Recursive parameter values are not allowed, for example .Param N = N+1.

- You may pass unused parameters, however, each parameter that is used within an expression must be assigned a value or have a default value.

- Parameters passed into subcircuits must be accounted for with .PARAM statement(s), put on the subcircuit call line in curly braces or appear in the subcircuit's default listings.

- Expressions to be evaluated in the .PARAM statements, in a part's property field, or in a subcircuit listing must also be placed inside curly braces.

- Default parameters are placed on the .SUBCKT definition line. All of the parameters should have defaults. If a default value is not available you can use "???" as a default.

- Parameters are available only within the subcircuit definition in which they appear. If a .PARAM is defined in the main netlist it is available in all subcircuits.

- Passed parameters will take precedence over default parameters.

Error checking

PARAM provides error checking that is limited to parameter evaluation problems. Error messages are displayed on the screen, and in some cases are inserted in the .CKT file.

Parameterized Expressions

Parameters or Expressions using parameters must appear within curly braces " { } "in order to be evaluated. For example;

```
.Subckt sub 1 2 PARAMS: Rval=1
Rval 1 2 {Rval}
.ends
```

In the above subcircuit the variable Rval within the curly braces will be substituted with a value of 1. The reference designator will be unaffected.

```
.Subckt sub 1 2 PARAMS: PARAM1=2u
X1 1 2 3 NextSub PARAMS: VAR1 = PARAM1
.ENDS
```

In the above subcircuit, the variable PARAM1 within the curly braces will be substituted with 2u. The parameter PARAM1 for subcircuit NextSub will not be modified. Likewise,

```
.Subckt sub 1 2 PARAMS: PARAM1=2u
X1 1 2 3 NextSub {VAR1 = PARAM1}
.ENDS
```

should produce the same results.

Local subcircuit parameters (PARAMS: or .PARAM) supersede global parameters (.PARAM parameters defined in the main netlist) of the same name.

Expressions in the main circuit are treated the same as expressions in subcircuits. Expressions can take the form of a mathematical equation or an If-Then-Else expression and can contain parameters, algebraic operators, a number of predefined math functions as described in the B element syntax.

Main Circuit Expression Examples;
R2 1 0 {Rnom/2}
C3 2 0 {V*psch*psch/beta} ic={p0/psch}
.MODEL Diode D IS={V1-I1/(V2-I2)} BV={Vmax*1.5}

Where Rnom, V, psch, and beta are defined in a .PARAM statement.

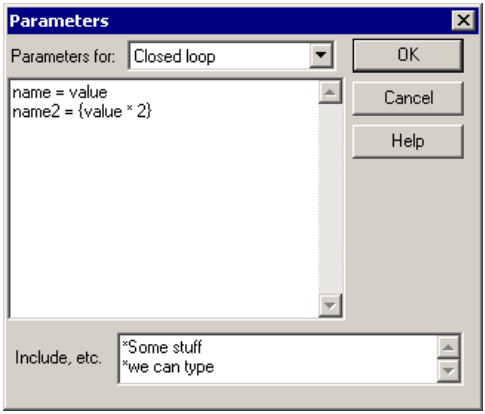
In R, L, C, and B elements parameterized expressions can be used inside of the behavioral equations. This allows you to mix parameters with circuit quantities like voltages, currents, and device power dissipations. For example;

R1 1 0 R= {p0-pvac} * ({vtot}-v(100)^{gamma})
B1 1 0 V = {Tr}*v(tm1) + {Ts-Tr}*v(tm2)

Note the use of the R=, C= etc., when an equation is utilized that contains a circuit/simulation dependent quantity.

Entering .PARAM Statements

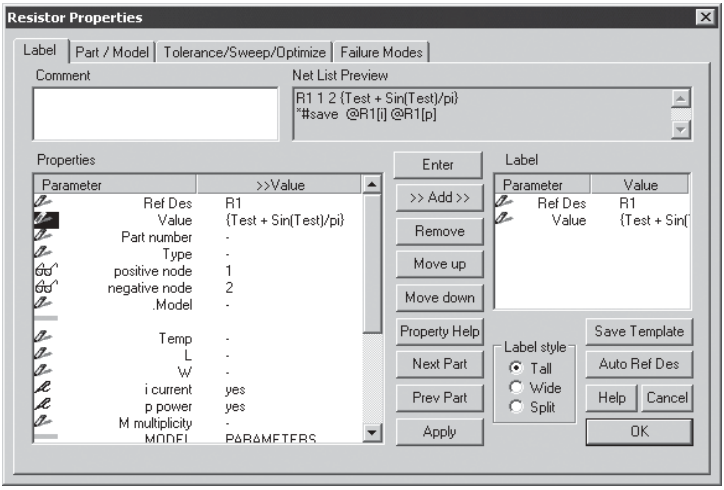
.PARAM statements can be entered in the Simulation Setup dialog in the User Statements area or in the Parameters Advanced Setup Options in the ICAPS Simulation control dialog as shown below. All statements entered into these dialogs will appear in the IsSpice4 netlist.



Entering Parameterized Expressions

To enter a parameterized expression in a numeric property field

- Click in the desired field.
- Enter the expression. Make sure the proper syntax is used and that you place the curly braces properly around parameters and expressions.



Normally, any Properties field that accepts a numeric value (part value, model parameter) can except a parameterized expression.

Note: For this example, the Test and PI parameters must be defined in a .PARAM statement. The is done in the Parameters Dialog. The Parameters Dialog is accessed from the ACTIONS menu ICAPS Simulation Control dialog under the Advanced Setup Options section.

Passing Parameters To Subcircuits

Subcircuit calling statement syntax:

Xname N1 N2 ... N# subname
+ {P1=*val1* or *expr1* ... Pj=*valj* or *exprn*}

where P1 through Pj are parameters passed to the subcircuit.

There are two ways to pass parameters into a subcircuit.

a) Parameters may be defined with a .PARAM statement either in the main circuit (ICAPS Simulation Control dialog Parameters Dialog) or inside the .SUBCKT netlist. If .PARAM statements are located in both places, the .PARAM statement in the subcircuit netlist takes precedence.

b) By stating the parameters on the subcircuit call line (X line).

The following forms are all valid.

```
x1 1 2 3 Subname {var1=expr var2=val2 … varn = valn }

x1 1 2 3 Subname {var1=val1 var2=expr …
+ varn = valn}

x1 1 2 3 Subname
+ {var1=val1 var2=val2 … varn = valn }

x1 1 2 3 Subname PARAMS: var1=val1 … varn = valn

x1 1 2 3 Subname PARAMS: var1=val1 var2=val2 …
+ varn = expr

x1 1 2 3 Subname
+ PARAMS: var1=val1 var2=expr… varn = valn
```

Note: A parameter can be a single parameter or a parameterized expression. However, the parameters must be previously defined in a .PARAM statement or in the subcircuit that the subcircuit call line is used in, so that a value can be passed to the subcircuit.

Parameters can be passed through multiple levels of a subcircuit's hierarchy. For example,

```
.PARAM Varmain = 1, Varmain2=1
.SUBCKT Subname 1 2 3
x1 1 2 3 Subname2 {var1=varmain }
.ENDS

.SUBCKT Subname2 1 2 3
x1 1 2 3 Subname3 {var2=var1 var3=varmain2}
.ENDS
```

Any number of variables can be accommodated. .PARAM expressions are evaluated before the passing function is called if possible. Any number of continuation lines can be used.

To enter a value for a passed parameter using SpiceNet

- Click in the desired field in the subcircuit's properties dialog.
- Enter the value. Select Apply or OK.

??? indicates that a value must entered. The default parameter value will be listed next to the parameter if one is available.

Default Subcircuit Parameters

Default subcircuit parameters can be predefined on the subcircuit definition line. If a value is passed in by the calling X line, it will override the default value. Defaults can appear in curly braces on the .Subckt line or after the "PARAMS:" keyword.

Syntax: .SUBCKT subname N1 ... N# {DP1=val1 ... DPj=valj}
.SUBCKT subname N1 ... N# {DP1=expr}

where D1 through Dj are default parameters, val# is a valid SPICE number, and expr is a valid expression. Curly braces around an expression in the default list are optional.

Example: .SUBCKT XFMR 1 2 3 4 {RATIO=1}

SpiceNet Notes: If "???" (3 question marks) are used as a default parameter, then 3 question marks will appear in the part's properties dialog in SpiceNet and the user will be forced to enter a value before the part can be simulated.

It is also important that each parameter be represented by a default value or set of 3 question marks. SpiceNet uses the defaults to compile a list of the available parameters for the part's properties dialog. If a parameter is not represented in the default list it will not be shown in the properties dialog.

Below are some examples of different syntax variations:

Expressions used in conjunction with the PARAMS: keyword must be surrounded by curly braces.

```
.Subckt Subname 1 2 3 {var1=val1 var2=expr … varn=valn}

.Subckt Subname 1 2 3 {var1=??? var2=val2 …
+ varn=valn}

.Subckt Subname 1 2 3
+ {var1=val1 var2=val2 … varn=valn}

.Subckt Subname 1 2 3
+ {var1=val1 var2=val2 …
+ varn=???}

.Subckt Subname 1 2 3 PARAMS: var1={expr} var2=??? …
+ varn=valn

.Subckt Subname 1 2 3 PARAMS: var1=val1 var2=val2 …
+ varn=valn

.Subckt Subname 1 2 3
+ PARAMS: var1=expr var2={expr} … varn=valn

.Subckt Subname 1 2 3
+ PARAMS: var1=val1 var2=val2 …
+ varn=valn
```

Parameter Passing Example

As an example, we will consider a semiconductor resistor subcircuit model. The subcircuit call is;

```
X1  1  2  RSUB {WIDTH=10U RPERSQ=1KOHMS}
```

The subcircuit contains;

Netlist Before PARAM

```
.SUBCKT  RSUB 1  2 {WIDTH=2U}
R1  1  2  {RPERSQ * (WIDTH^2)/1E-12}
.ENDS
```

The subcircuit call, X1, calls the subcircuit and passes two parameters, WIDTH and RPERSQ, into the subcircuit. The resistance value R1 will be calculated based on the equation that is shown next. After running a simulation, all of the extended syntax is transformed into IsSpice4 syntax by evaluating the expression(s) and then replacing each one with a value. For example;

```
X1  1  2  RSUB#0
*{WIDTH=10U RPERSQ=1KOHMS}
```

Netlist After PARAM

```
.SUBCKT  RSUB#0 1  2
R1  1  2  100.00K
.ENDS
```

The passed parameters are left in the final IsSpice4 input file on a comment line below the subcircuit call. After a simulation is run, the subcircuit names will have a sharp sign and a number appended to them in order to make them unique.

If two RSUBs are called with different sets of parameters, then two different subcircuit representations will be created automatically. For example:

```
X1 1  2 RSUB {WIDTH=50U RPERSQ=100OHMS}
X2 3 4  RSUB {WIDTH=10U RPERSQ=1KOHMS}
```

will produce:

```
X1 1 2  RSUB#0
*{WIDTH=50U RPERSQ=100OHMS}
X2 3 4  RSUB#1
*{WIDTH=10U RPERSQ=1KOHMS}

.SUBCKT RSUB#0  1  2
R1 1 2 250.00K
.ENDS
.SUBCKT RSUB#1  1  2
R1 1 2 100.00K
.ENDS
```

Each subcircuit call with a different parameter list will automatically create a new subcircuit. If all subcircuit calls use the same parameter list, only one subcircuit will be generated for all calls.

DEFINE

DEFINE allows a text string to be replaced with another text string within the netlist. This function can be used to easily change model names that are used numerous times, or to easily shorten long phrases.

Syntax:

*DEFINE *variable name* = *substitute text string*
*DEFINE *variable name* = /*substitute text string*

Example:

*DEFINE DUT=MPSA42

In the example, every occurrence of the string “DUT” will be replaced by its substitute text string “MPSA42”. The expression “substitute text string” may contain any characters. The substituted text is comprised of all the characters following the “=” equals sign up until a carriage return is encountered.

*DEFINE statements are erased as they are performed, in order to eliminate duplicate substitutions, unless a forward slash is placed before the substitute string. The Define keywords are erased by changing the “D” in the *DEFINE to a lower case “d”. If there are *DEFINE statements inside any subcircuits, the DEFINE statements in the deepest subcircuits are processed and removed first.

The “/” causes the define string to apply to the entire netlist rather than for only one include pass, resulting in a “global define”.

The IsSpice4 comment delimiter, *, is used to make the INCLUDE and DEFINE commands compatible with IsSpice4; that is, it remains in the netlist, but is ignored when an IsSpice4 analysis is run.

The DEFINE function is run whenever the INCLUDE program is run.

DEFINE Rules and Limitations

Define is part of the ICAPS program.

- DEFINE statements are only processed in a forward direction. Define statements are usually placed at the beginning of the netlist in order to apply them to all subsequent entries.
- Be careful of what you are substituting. The variable name must be unique so that inadvertent substitutions are avoided.
- The variable name cannot start with a number.
- The DEFINE statement cannot longer than one line long.
- All characters before the “=” must be found.
- All characters following the “=” sign, the substitution string, will be replaced.

DEFINE Example

To use a *DEFINE statement;

- Place a *DEFINE statement in the input netlist.

Example:

Define Syntax

```
*DEFINE WIDTH=5U
```

- Place the word WIDTH in the netlist.

Example:

Before DEFINE

```
M1 1 2 3 4 WIDTH
M2 7 8 9 10 WIDTH
M20 34 45 23 12 WIDTH
```

- Select the Simulation Control... function from the ICAPS ACTIONS menu. Make sure the “Include Libraries” option is checked in the dialog.

- Perform a simulation.

The DEFINE function will be run automatically before the INCLUDE function is run. After the netlist preprocessing is finished, the netlist will be submitted to IsSpice4.

After DEFINE

```
M1 1 2 3 4 5U
M2 7 8 9 10 5U
M20 34 45 23 12 5U
```

The defined string WIDTH was substituted with the definition that was given in the *DEFINE statement.

INCLUDE

See Working with Model Libraries or the on-line help, for more info on constructing model library files.

The *INCLUDE statement is used to access models or subcircuits that are located in a library file, or insert an entire file into the netlist. In general, the schematic program will include the subcircuits and models for all top-level components in the SPICE netlist it produces. Additional INCLUDE statements are normally only required when other nested subcircuits and models must be included. In this case a *INCLUDE statement should be inserted into the subcircuit entry after the .ENDS line.

When a simulation is run, the INCLUDE function searches the referenced library (extension .LIB) and places the appropriate models and subcircuits into the netlist automatically. If the extension is anything but .LIB, the entire contents of the file will be inserted just after the *INCLUDE line. The INCLUDE feature is only active when the “Include Libraries” option is checked in the ICAPS Simulation Control Advanced dialog.

Syntax: ***INCLUDE** *filename*.lib
***INCLUDE** *filename*.xxx

Example: *INCLUDE USER.LIB

Note: The following items are necessary for INCLUDE to operate;

- The proper call statement for the device must be used. (i.e. A, C, D, J, M, O, Q, R, S, W, etc. or subcircuit, X)
- A *INCLUDE statement must be present and must point to the library that contains the called devices.
- The “Include Libraries” option (default on) must be activated.

Note: Note: If you find that you specify the same simulator options over and over, then you can do the following procedure.

Bring up IsSpice4 Simulation Setup dialog. Uncheck all analysis except for “Simulator Options...” Press “View All Controls...” button then copy and paste all .options statements into a text file, i.e., myoptions.txt. In the User Statement window add either

(1) *INCLUDE myoptions.txt

(2) *INCLUDE c:\spice8\myoptions.txt.

If you don't specify an absolute path, then the .txt file must be located in the same folder as the DWG file.

INCLUDE Example

As an example, consider the following call to a 2N2222 BJT.

Q1 10 15 20 QN2222

Model Call

The model name, QN2222, is the name of the library entry that contains the description of the transistor. The model is located in the library BJTN.LIB.

The *INCLUDE BJTN.LIB statement would retrieve the model from the BJTN library;

```
SAMPLE NETLIST
*INCLUDE BJTN.LIB
.DC VCE 0 15 .5 IB 100U 1M 100U
.PRINT DC I(VC)
IB 0 1
Q1 2 1 0 QN2222
VC 3 2
VCE 3 0
.END
```

Netlist Before INCLUDE

When the simulation is run, the model library BJTN.LIB will be searched, for the QN2222 model statement, which will be inserted into the final netlist.

```
SAMPLE NETLIST
*INCLUDE BJTN.LIB
.MODEL QN2222 NPN (IS=15.2F NF=1 BF=105 VAF=98.5 IKF=.5
+ ISE=8.2P NE=2 BR=4 NR=1 VAR=20 IKR=.225 RE=.373 RB=1.49
+ RC=.149 XTB=1.5 CJE=35.5P CJC=12.2P TF=500P TR=85N)
* Motorola 30 Volt .8 Amp 300 MHz SiNPN Transistor
.DC VCE 0 15 .5 IB 100U 1M 100U
.PRINT DC I(VC)
IB 0 1
Q1 2 1 0 QN2222
VC 3 2
VCE 3 0
.END
```

Netlist After INCLUDE

Important Note: The Include operation is normally completed AUTOMATICALLY by the schematic entry program. You do not have to type *INCLUDE statements.

INCLUDE Rules and Limitations

When INCLUDE is run, the netlist is loaded and the specified libraries are searched for unresolved subcircuit or model references in the order in which they appear in the netlist. Each library will be searched repeatedly until no additional references can be resolved in that library. The process is then repeated for succeeding libraries. The program runs until a pass is made with no unresolved references.

Libraries may cause additional unresolved references to occur if your subcircuits call other subcircuits or models. It is best to resolve those references within the same library.

The following guidelines should be observed when using the Include feature:

- A *INCLUDE statement is REQUIRED if your subcircuit calls other subcircuits or models.
- A *INCLUDE statement must exist in order to extract a model from a library.
- The library (.LIB) file must conform to the format as discussed later in this chapter.
- *INCLUDE statements may be placed within subcircuits, but all nested subcircuits should be located in the same library.
- The subcircuit or model is inserted into the netlist, starting at the ".SUBCKT" or ".MODEL" line, and encompasses all text prior to the next row of five asterisks.
- Only one INCLUDE statement is required for each library.
- The "Include Libraries" option in the ICAPS Simulation Control Advanced dialog must be activated.

Subcircuit and Model Hierarchy

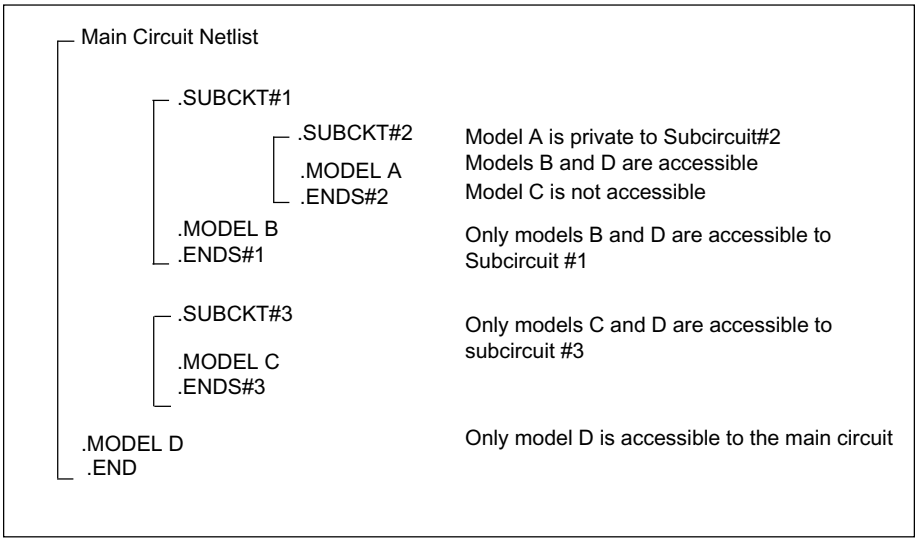
IsSpice4 subcircuits and models can be used within a circuit hierarchy. The rules by which subcircuits and models are found when they are called from your source netlist allow subcircuits to contain private subcircuit and model names. That is, a model or subcircuit contained within a hierarchy is exclusive to that hierarchy and cannot be used by another. This concept allows you to build complex circuits without having to worry about using the same names in different subcircuits.

When a subcircuit is called, IsSpice4 will first search within the calling subcircuit for any subcircuit reference, then it will search back one level, if any, to the calling subcircuit and then through other subcircuits until it reaches the location where the original call was made. The same rule is applied to model statements. You can look at the hierarchy as a tree with branches, similar to a DOS directory tree.

The subcircuit search extends to other subcircuits on the same branch, but not for models or subcircuits that are within other subcircuits on the same branch. When a subcircuit calls another subcircuit, the references (models, subcircuits and elements) in the called subcircuit are private and therefore cannot be referenced by the calling circuit.

The concept of a hierarchy allows you to reuse a model or subcircuit for different parts of your circuit, providing accessibility problems have been eliminated. IsSpice4 will internally flatten the hierarchy so that there is a separate entry for each instance of a device.

Libraries can contain unresolved references, for example, a subcircuit could reference a model or another subcircuit that is in a separate library. It is best to resolve these nested groupings within the library in order to simplify debugging and speed the processing by INCLUDE.


Main Circuit Netlist
.SUBCKT#1
.SUBCKT#2
.MODEL A
.ENDS#2
Model A is private to Subcircuit#2
Models B and D are accessible
Model C is not accessible
.MODEL B
.ENDS#1
Only models B and D are accessible to Subcircuit #1
.SUBCKT#3
.MODEL C
.ENDS#3
Only models C and D are accessible to subcircuit #3
.MODEL D
.END
Only model D is accessible to the main circuit

Extended Analysis

Introduction

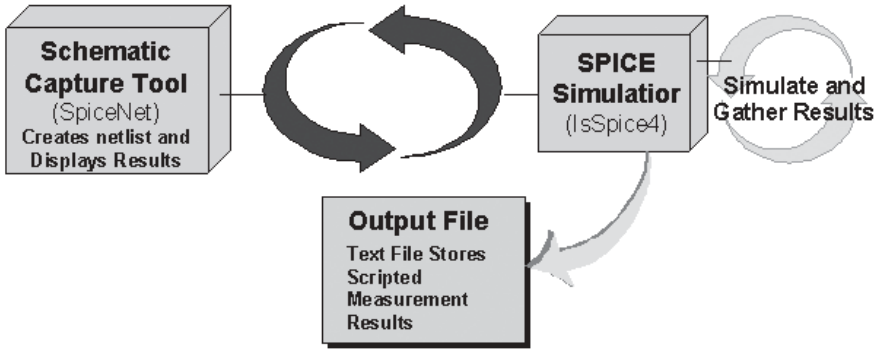
This chapter deals with the process of performing Monte Carlo Analyses, Circuit Optimization, Parameter Sweeping and Simulation templates in general. Examples are given in order to explain these analyses.

The Monte Carlo, Optimization, Parameter Sweeping and Failure analyses are NOT available in ICAP/4Rx.

Monte Carlo analysis is the evaluation of circuit performance based on the statistical variations of parameter tolerances. Monte Carlo analysis is vital to predicting how a circuit, whose component values vary in the real world, will perform when it is actually fabricated.

Monte Carlo analysis can be run using either of two methods. The first method is selected using the “Monte Carlo” radio button in the “Simulation Control Dialog.” To get meaningful information from this method, you must define one, or a series of measurements, before running Monte Carlo . This method is mainly used to obtain the mean and 3-sigma tolerances available for setting measurement pass-fail limits. Pass-fail limits are displayed in the “Measurement Results” dialog after simulation, and they are setup using the “Set Measurements Limits” dialog. See the Getting Started manual, tutorials #6, #7, and #8 for a detailed description of these features.

The second Monte Carlo simulation method employs simulation templates and is run by first selecting the MONTE item in the “Simulation Template” list box. You can elect to make measurements either before of after running the simulation. If you define electrical measurements before running the simulation, then you can set pass-fail test limits in Simulation Control’s “Results” dialog. The simulation template will run IsSpice just one time, while varying tolerances and repeating simulations and collecting data in a series of IsSpice4 plots. When completed, the Monte button will be enabled in IntuScope’s “Add Waveform” dialog. Tutorial #6 in the Getting Started manual shows how the data can be viewed. This Monte Carlo simulation technique is useful for obtaining graphical data in IntuScope for the statistical runs, a feature not available with the first Monte Carlo method.



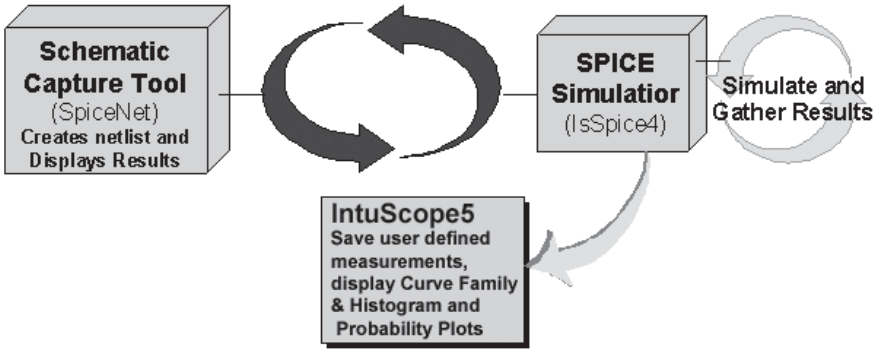
The diagram shows the general program flow for Monte Carlo analysis using Method #1 ICL scripted measurements.

This method uses an ICL script to analyze the output from each case run. The results are generated and sent to the schematic for display in the Results Dialog.

Circuit Optimization provides the ability to optimize multiple parameters for virtually any single circuit objective function. Any IsSpice4 parameter, including component and model parameter values, can be varied in an attempt to minimize an user-defined objective function.

Parameter Sweeping is similar to a DC sweep but you are able to sweep any two circuit parameter instead of just DC voltages. If you just want to sweep only one primitive part like resistor, capacitor, inductors, voltage/current source, or even the global circuit temperature then you can use the Alter tool (from SpiceNet) to create a curve family. With Parameter Sweeping, a component value or parameter is stepped and an IsSpice4 simulation is performed for each value. The simulation results from each run are available for plotting, so you can perform complex manipulations on the output data (rise/fall time, propagation delay, etc.), and plot any measured value against the parameter that was swept.

Simulation Templates provide the ability to perform various analyses, and process the simulation results. These were invented by Intusoft to integrate ICL scripts with the netlist building function in SpiceNet. Simulation templates eliminate repetitive tasks and save a significant amount of time.



The diagram shows the general program flow for Monte Carlo analysis using Method #2 Simulation Templates.

This method is used if you want to create a curve family or use IntuScope to process the simulation results of each case.

Tolerances

Tolerance Distribution Notes

Statistical analysis is a convenient although brute-force method of finding the envelope of a circuit's performance. Analysis performed using statistical simulation has become known as Monte Carlo analysis. The advantage that Monte Carlo analysis has over other estimation techniques is that it is not affected by non-linearity or local minimums that confound sensitivity or envelope-based simulations. Moreover, Monte Carlo analysis can be performed in a parallel fashion in order to achieve processing speed increase.

In order to perform statistical analysis, a repeatable method for generating random numbers is used. The need for repeatability arises to enable simulation lots/case trials to be performed using parallel computing techniques.

The random number generators that Intusoft has developed for its IsSpice4 use an integer-based system. The Intusoft generators use a software implementation of tapped shift register with "polynomial" feedback to generate a series of numbers that repeats after 2^n -1 terms, where n is the number of bits. There are two pieces of information that determine the sequence of numbers; these are the seed number, or starting point, and the generating polynomial. Given a generating polynomial, these generators produce a random sequence that has very low cross correlation; that is, the sum of products which start with a different seed show a very small cross correlation. Furthermore, there's no correlation between random sequences made using different generating polynomials. For purposes of this discussion we will define random generators that produce uncorrected sequences as orthogonal.

Monte Carlo analysis is commonly performed using a lot/case approach. This allows components within the lot to be matched more closely than those between different lots. This characteristic is used widely in integrated circuits and systems to achieve precision that couldn't otherwise be achieved. To build random generators, it is then necessary to initialize the lot and case generators for each type of part so that the subsequent pattern will be orthogonal. The basic trick is to advance a generator from a known seed by the desired number of lots or cases and then to make a new orthogonal generator using the resultant random number to select the new generating polynomial. Then each lot generator and each case generator is orthogonal and the system of generators for any given lot or case can be reproduced by any other platform performing the same simulation.

Given a shifting word length, not all generating polynomials will produce a maximum length sequence. Those that produce a 2^n - 1 sequence are then mapped from the n bit word into a smaller space. If the same polynomial generator is used more than once, than an unused generator will be selected to prevent inadvertent correlation.

To handle different distribution functions, the distribution model used for lot/case statistics also allows three distribution functions.

They are normal or Gaussian, binary, and uniform.

The tolerance for each of these has a meaning shown in the table below.:

Distribution	Standard Deviation as a function of TOL	Comment
Normal	Tol/3	Tol is 3 Sigma
Binary	Tol	Result is +Tol or -Tol
Uniform	2*Tol/sqrt(12)	Equal probability from -Tol to +Tol

	Normal	Binary	Uniform
1 sigma	Tol/3	Tol	2*Tol/sqrt(12)
1 sigma/Tol	.333	1.0	.577
3 sigma/Tol	1	3	1.73

The last entry, 3 sigma/Tol is what is reported in the Results dialog.

The value used for Tol is different for each distribution. For linear combinations results tend to be normally distributed with dependence on the one sigma or RMS of the selected distribution. For linear cases, the RMS of the distributions to correspond to the results of the our RSS analysis. When an extreme value analysis (EVA) warns that the sign of sensitivity is different at the extremes, it is better to rely on Monte Carlo results instead of EVA or RSS.

Working With Tolerance

Tolerances can be entered as a percent (e.g. 10%) or as an absolute value (e.g. .314). Tolerances define the 3 sigma points for the specified distribution (default Gaussian). You can specify both lot and case tolerances using the .TOL statement. If you do then the simulator will compute a lot tolerance (once for each lot) and the sum (the case tolerance for each simulation case).

Lot and case tolerances are set in the Part Properties dialog for a specific device. You can create an indirect Lot/Case tolerance reference name in the ”Tolerance Definitions” dialog. This is brought up by clicking on the tolerance button located in the Advance Setup Options section of the Simulation Control dialog.

Example of the tolerance format:

IsSpice4 Statement	±3 sigma value
R1 1 2 1K TOL=10%	.900K to 1.1K
R2 3 4 .01 TOL=.001	.009 to .011

.MODEL TRAN NPN (BF=100 TOL=10% ...)
gives BF between 90 and 110

Note: The distinction between a percentage tolerance and an absolute value tolerance is very important. An error in the declaration of a tolerance will lead to unexpected results.

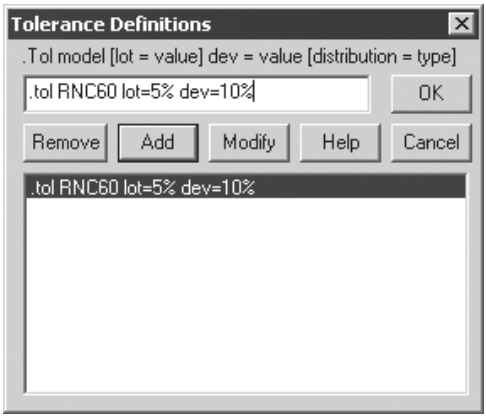
To place a tolerance on a device or model parameter:

- Double click on the part in the schematic to open its Properties dialog. Click on the Tolerance/Sweep/Optimize tab toward the top.
- Click on the Lot or Case field for the desired parameter.
- Enter a tolerance. Don't forget the required % character if the tolerance is a percentage. Select OK.

To create an indirect Lot/Case tolerance name:

Tolerances are evaluated when each Monte Carlo analysis case is performed.

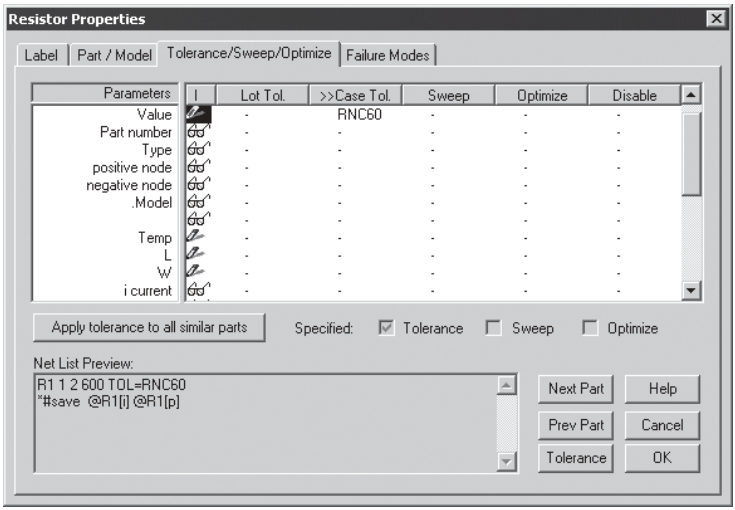
- Open the ICAPS Simulation Control dialog from the Actions menu in the schematic. Click the Tolerance box toward the bottom.
- Enter ".Tol name Lot=#1% Case=#2%" into the text field. Here, Name is tolerance reference name, and #1 and #2 are the Lot and Case percentages.
- Click the Add button. An example is shown.
- Click OK.



To use the indirect Lot/Case tolerance name:

Tolerances correspond to the 3 sigma (± 99.87%) value.

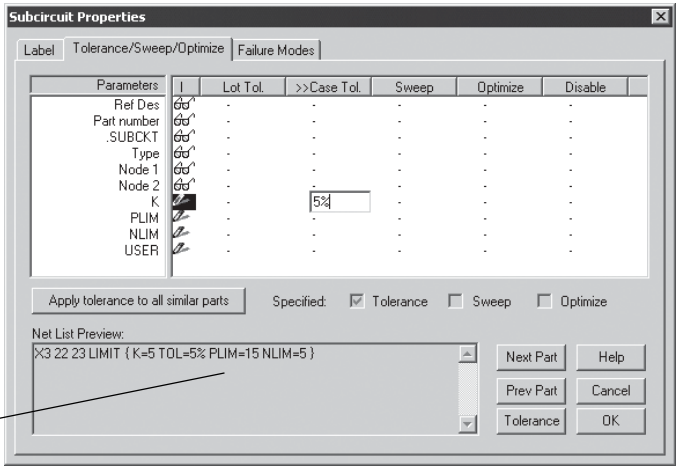
- Double-click on a part. Select the Tolerance/Sweep/ Optimize tab.
- Click on the Case field for the desired parameter.
- Enter the tolerance name. Click OK. An example is shown next.



Subcircuit Parameter Tolerances

In some instances, it may be necessary to place tolerances on parameters that are passed to subcircuits.

Don't forget the required % character.



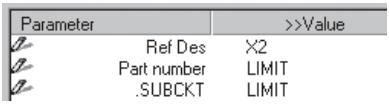
Notice that the tolerance value appears here.

To place a tolerance on a passed subcircuit parameter:

- Double-click on the part, click on the Tolerance/Sweep/Optimize tab. Select the desired passed parameter and enter a tolerance.

To place a tolerance on a subcircuit parameter that isn't passed-in:

- Double-click on the part. In the Label tab, double-click on the value field beside the .SUBCKT parameter.



- Enter the desired tolerance value in the Edit Subcircuit dialog, directly beside the subcircuit parameter value that you want to tolerance.

Varying Subcircuit Tolerances

It may also be advantageous to make a component into a subcircuit in order to scale the component tolerances more easily.

Example:

The partial netlist below shows the subcircuit MIRROR, which has two resistors that are assigned tolerances. For subcircuit X1, we will produce a Lot/Dev distribution. For subcircuit X2, we will simply provide a device tolerance for each resistor value.

Change this:

```
SAMPLE NETLIST
X1 1 2 MIRROR
X2 5 6 MIRROR
*****
.SUBCKT MIRROR 1 3
R1 1 2 1K
R2 2 3 1K
.ENDS
```

Components getting tolerances

To this:

```
.PARAM R1T=1K Tol=10% R2T=1K Tol=5%
.TOL NRES LOT=30% DEV=2%
X1 1 2 3 MIRROR {R1=1K Tol=NRES R2=1K Tol=10%}
X2 5 6 8 MIRROR {R1=R1T R2=R2T }
.SUBCKT MIRROR 1 2 3
R1 1 2 {R1}
R2 5 6 {R2}
.ENDS
```

Format to pass toleranced parameters

.TOL and TOL= syntax can be used together in the same circuit, if necessary.

In the example, R1 and R2 in X1 will be given a value that is adjusted by the tolerance before they are passed into the subcircuit. Each time the mirror subcircuit using these parameters is called, a different subcircuit representation will be automatically created with different values for R1 and R2. This is because the resistors will each have a different value and a different ratio, both dependent on the statistics. For X2, all of the R1 and R2 values for all the subcircuits that use the .PARAM parameters will have the same values.

Monte Carlo Using Scripted Measurements: Setting the Param After Monte switch is not necessary when performing scripted (non simulation-template) Monte Carlo analysis. All subcircuit descriptions are given unique statistics.

Tolerance Value Generation

The default random number generator makes a Gaussian distribution by summing 12 uniformly distributed random numbers, a process that tends to produce a Gaussian distribution according to the Central Limit Theorem of probability theory.

Monte Carlo Analysis (Not Available in ICAP/4Rx)

Performing a Monte Carlo analysis begins by developing a working circuit description. After making sure that the circuit topology is correct, component or model parameter value(s) may be given a tolerance. The tolerance corresponds to the 3 sigma (± 99.87%) value that the parameter may take on under real world conditions. During the analysis, parameter values will be toleranced based on a Gaussian statistical model.

Initially, a standard simulation run is performed. The circuit simulation is described as standard because all of the component values will be at their nominal levels. Then you must define what type of measurements you want to record during the analysis.

The statistical analysis of the circuit is performed by building the circuit description repeatedly using different parameter values for the toleranced components or model parameters. Each circuit is simulated by IsSpice4 and then analyzed by the user-defined measurements. After all of the circuits have been simulated, the results can be viewed in the Results dialog, selected inside the Simulation Control Dialog (if you chose scripted measurements).

Performing A Monte Carlo Analysis (ICL Scripted)

The following steps will guide you through the actions necessary to perform a standard Monte Carlo analysis. The following is a general explanation.

STEP 1: A Working Circuit

Start ICAPS and obtain a working version of the circuit. Note that if a particular case does not simulate to completion during the Monte Carlo analysis, the result will not be used in the final statistics.

STEP 2: Adding Tolerances

The next step is to place tolerances on the parameters that you optionally may wish to vary, in lieu of the default variation ascribed during a scripted Monte Carlo analysis. Any value, component values, model parameters or parameters passed into a subcircuit, can have a tolerance. Tolerances are placed in the Tolerance/Sweep/Optimize tab in the Part Properties Dialog.

STEP 3: Setting Up The Measurements

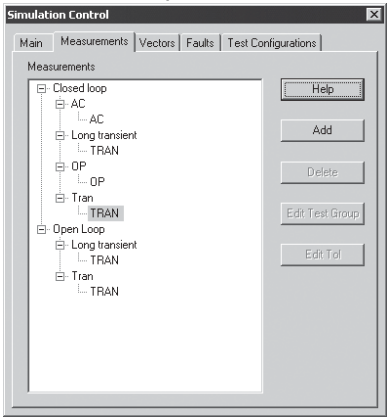
Before a Monte Carlo analysis can be run, it is recommended that you decide what measurements to record. These are setup using the Measurement wizard in the Simulation Control dialog. Most measurements (i.e., rise time, max, pk-to-pk) are set up with just a few mouse clicks. You also have the ability to write your own ICL scripts to make a measurement. (See Chapter 11)

Note: Advanced analysis details are covered in the schematic's on-line help. You can view this by pressing F1 when any Measurement Wizard dialog is displayed. For non simulation-template Monte Carlo, only the mean and 3 sigma value of each measurement will be calculated, and no waveform data is provided. .

Open up sample.DWG in the folder :\spice8\SN\sample2

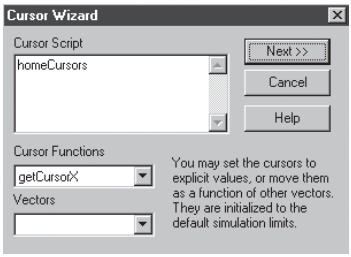
To setup a Monte Carlo Scripted Measurement

- Select the ICAPS function from SpiceNet's Actions menu.
- Select the Measurements tab.
- Select the configuration and analysis type you want to add a measurement to. For example, select Closed Loop, TRAN.



- Click the Add button to add a measurement. This will start the Measurement Wizard.
- Make sure the proper Simulation, Configuration, Setup and Method entries are selected. Click Next. The example screen images show TRAN, Closed loop, TRAN, and Function, respectively.



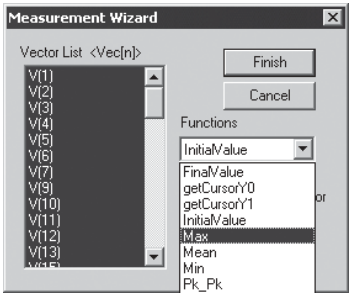


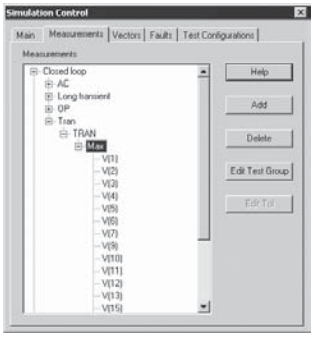
- Click the Next button to display the Cursor Wizard dialog.

The Cursor Wizard dialog allows you to position cursors to make cursor relative measurements. It starts with the command "homeCursors," which sets the cursors at the beginning and end points of the analysis (x axis: in this case with TRAN selected as the analysis). For this overview, we will leave the cursors at the default locations and make a measurement that includes the entire X axis span.

- Click the Next button to go to the final Wizard dialog.

In this dialog you can select which voltages, currents, and power dissipations you want to record. The example shows several voltages.





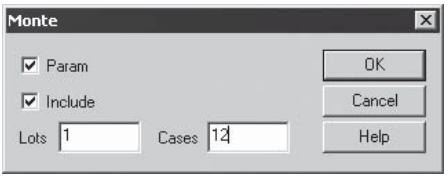
- Select the waveforms you want to measure from the Vector List.
- From the drop-down list under functions, select the type of measurement you would like to make on all of the selected waveforms. You can add as many different measurements on different vectors, as desired.
- Select "Finish" when done, then select the Main tab in the Simulation Control dialog.

The pictures to the left show several voltages selected along with the max function. The final Measurements tab settings are shown below it.

STEP 4:Defining Lots and Cases

To define how many lots and cases to run

- Select the ICAPS function from SpiceNet's Actions menu. Select the Main tab on top.
- Click on the "Monte" box located toward the bottom.



- Enter a value in the "Lots" field.
- Enter a value in the "Cases" field, (i.e., 12). The number of simulations run is equal to Lots * Cases.
- Click on the OK button to close the Advanced Settings dialog.

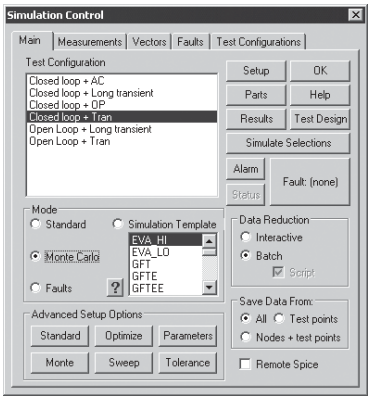
The Monte Carlo analysis will create the proper number of circuit instances based on the number of Lots and Cases. For example, Lots=2 and Cases=4 will cause 8 circuits, each with different tolerances, to be simulated.

STEP 5: Running a Monte Carlo Simulation

The Monte Carlo analysis is run from the ICAPS Simulation Control dialog in SpiceNet.

To begin the Monte Carlo Analysis

- Click on the "Monte Carlo" radio button in the Simulation Control dialog.



- Select the desired Test Configuration.
- Select the Batch radio button.

  The Batch radio button shuts off the IsSpice4 interactive waveform display, thereby improving simulation performance. The script checkbox causes all of the scripted measurements you have set up to be performed.
- Click on the Simulate Selections button.

- A dialog will be displayed, asking you if it is OK to perform the requested number of simulations. Select Yes if the number is correct.

You will see the Simulation Status as the analysis proceeds.

After the last case is simulated, you will be asked “Do you want to run a standard reference simulation.” This is a simulation with all of the parameter values set to their nominal values. Running this simulation can be useful if you will be setting test limits on your scripted measurements. If you are just reviewing the Monte Carlo statistics, you do not have to run the reference simulation.

- Select Yes or No as desired.

Viewing the Results

The mean and 3 sigma values are recorded for each measurement vector.

The measurements are automatically fed back to the SpiceNet program for display when the Monte Carlo analysis is finished (or aborted).

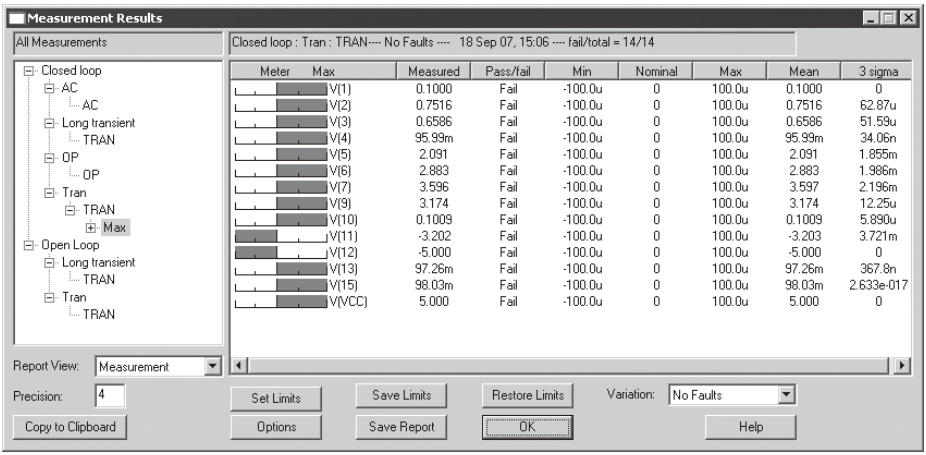
To view the scripted Monte Carlo mean and 3 sigma results

- Go to the ICAPS Simulation Control dialog.

- Click the Results button.
- Click one of the measurement names to see its results.

The Results dialog is used for looking at scripted measurement results. Scripted measurements and the Results dialog can be used for any analysis. Please see the “Monte Carlo and RSS Analysis” and “Design Validation and Automated Measurements” tutorials in the Getting Started book for more information.

For non simulation-template Monte Carlo analysis, there are data columns for the measured (last simulated) value, mean, and 3 sigma values.



The other columns, Meter, Pass/Fail, Min, Nominal, Max, are useful if you have set limits on the measured vector. Please see the on-line help (press F1 in the Results dialog) for more information on setting test limits.

You may have to scroll the dialog’s bottom bar to the right, and/or reduce or increase some of the column widths in order to see the mean and 3-sigma values. The latter step is done by left-mouse dragging the desired small vertical bar between any of the title tabs (i.e., min, max...). The Precision (low left corner) may have to be increased if readings are taken out to several decimal-point digits.

Circuit Optimization (Not Available in ICAP/4Rx)

The Intusoft Optimizer performs design optimization by trying to minimize (achieve) a design objective function (i.e., minimize a voltage, achieve a particular phase margin, etc.). Only circuit parameters with optimization percent value will be changed by the optimizer and only by the percent amount you specify. If you specify 30% on a resistor with an initial value of 1k then the optimizer will only change its value from 700 Ohms to 1.3KOhms.(30%*1K=300, 1K+300=1.3K and 1K-300=700) Also this optimize percent is not saved in the .DWG file so you will need to reenter it if you close the file and re-open it.

Note:Simulation Template Optimize performs 1 pass through the stepped optimization algorithm, and Optimize2 performs 2 passes. Choose Optimize2 if you want to optimize multiple parameters.

Optimizer Preparation

Specify objective function 'ofunc'

- Bring up ICAPS/Simulation Control...
- Click on the Measurements tab.
- Select the Test Configuration you want to optimize and press the add button.
- Select the Script Method, give it a name called 'ofunc', and press the next button.
- Enter the objective function you want to minimize.

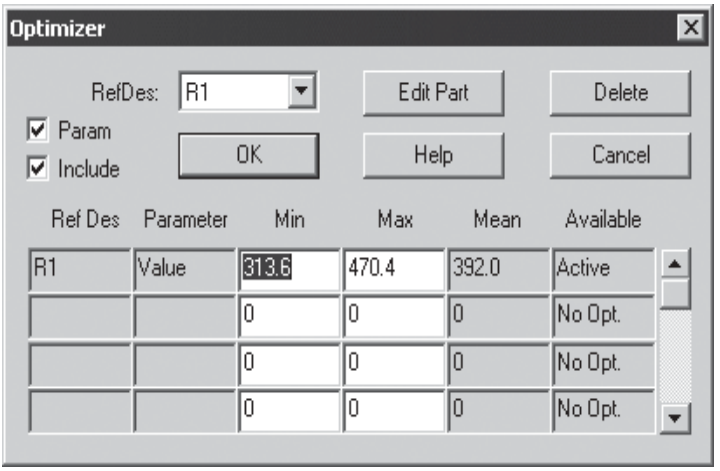
Example 1: [You want 5 Volts on Vout]
setcursor 0 150u
setcursor 1 400u
ofunc =(max(Vout - 5))^2

Example 2: [You want 90 degree phase margins]
setcursor 0 100
setcursor 1 10k
phase = phaseextend(phase(vout)-phase(vin))
ofunc = (min(phase) - 90)^2

It doesn't matter what you call the script measurement but you should only have one in that test configuration. We use 'ofunc' in our schematic examples. This script will be minimized so remember to square the equation to ensure that there is a min.

To specify optimize percentage

- In Simulation Control click on the “Optimize” button in the Advanced Setup Options section.
- Select the RefDes of the part you want to set a optimize constraint on and press the Edit Part button.
- Enter a percentage value in the optimize column for each parameter that you want to be optimized.
- Press the Ok button and the Optimize dialog will come up showing the min and max value. If you set a percent value on a parameter that is initially 0 or infinity, then it will come up as 0.



Running The Optimizer

The optimization process itself consists of measuring the objective function for a set of parameter values, and then finding the parameter value that minimizes (achieves) the objective function. OPTIMIZE is a single pass version and OPTIMIZE2 is a 2-pass version. If you are doing single parameter optimization to select a component value, then OPTIMIZE should work. If you are doing multi-parameter optimization, use OPTIMIZE2.The algorithm uses polynomial regression to make a high order curve fit so that it is possible to find a minimum value in the presence of local minimum values.

To run the Optimizer

- After you have specified all the parameters that you want to be optimized, press the Ok button to dismiss the Optimizer dialog.
- Under Simulation Templates select OPTIMIZE or OPTIMIZE2 and press the simulate selections button.

The circuit optimization will now begin. You will see the analysis proceed on the screen.

Single and Multi-Parameter Sweeps (Not Available in ICAP/4Rx)

Any single circuit parameter (up to two components) may be swept through a predefined range, using a symmetrical increment or decrement value.

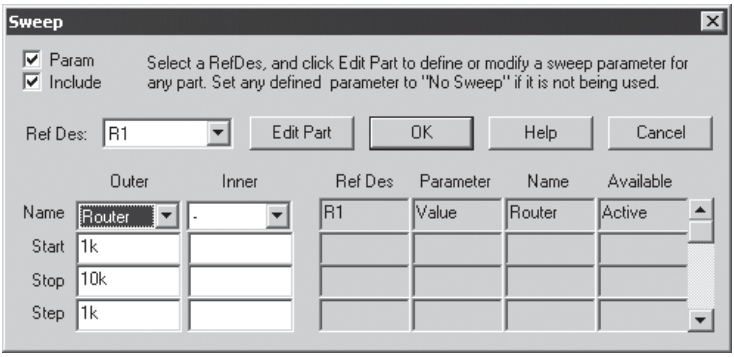
One way to prepare a part for a single device-parameter sweep

- Select a SpiceNet schematic drawing.
- Double-click on the part whose parameter will be swept.
- Click on the Tolerance/Sweep/Optimize tab atop.
- Select the desired parameter's value field, and enter the name of the variable, rather than a numerical value (e.g., "Rvary"), in the "Sweep" column.

VERY IMPORTANT NOTE: *the variable_name must NOT be set to a reference designation.* The sweep function directly substitutes the *Value* in place of the variable name. If a reference designation is used, it will be replaced with a number, and the IsSpice4 program will respond with an error.

Centralized method to sweep one or two components

- Select "ICAPS/Simulation Control" from SpiceNet's "Actions" pulldown menu.
- Select the "Sweep" function from the "Advanced Setup Options" box at the bottom.



"Sweep" dialog box from the Simulation Control dialog.

- Using any schematic, Select R1 from the "Ref Des" dropdown box shown above. Then, press the "Edit Part" box just above.
- Select the Tolerance/Sweep/Optimize tab atop the "Resistor Properties" dialog.
- Fill in the sweep variable name "Router" in the "Sweep" field. Note: if performing a dual (nested) sweep is desired, fill in an inner variable name in the "Sweep" field too. Press OK.
- Back to the Sweep dialog, enter the desired Outer loop Start, Stop, and Step values as shown in the pictorial above, then select the variable name(s) in the "Name" field(s).
- Click on the OK button to dismiss the Sweep dialog.
- Select "Sweep" in the Simulation Template list.
- Select the desired test configuration in its window above.
- Click on the Simulate Selections button to begin the analysis.

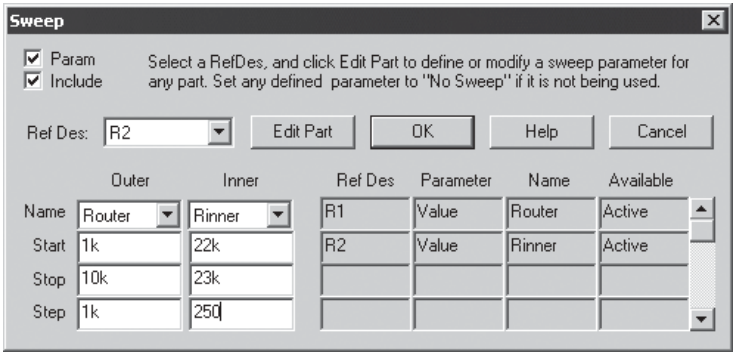
Sweeping two parameters

As mentioned, two parameters may be swept in a "nested" loop by using the same above procedure.

With a nested loop, the “inner” variable is stepped through its entire range, for each incrementally stepped value of the “outer” variable.

- In the Part Properties dialog, select the Tolerance/Sweep/Optimize tab. Again, this can be accessed from the Sweep dialog’s “Ref Des” pulldown and “Edit Part” box as shown below. Enter the second desired name of the variable to be swept, (e.g. Rinner), in the “Sweep” column. Press OK.

- Back to the Sweep dialog, enter the desired Inner loop Start, Stop, and Step values. Select the part’s variable name (e.g. Rinner) in the Name field. Run the Sweep Simulation Template as before.



Error Messages and Solutions

For a Monte Carlo, Circuit Optimization, or Parameter Sweep analysis to run, **each case must result in a valid simulation.** The Monte Carlo tolerances, and optimized/swept circuit variables, must produce circuits that converge and simulate without errors. If an error (non-convergence or IsSpice4 syntax error) occurs during an IsSpice4 simulation, the dialog “Spice aborted” will be displayed and the analysis will be halted.

If IsSpice4 runs out of memory, the “Spice aborted” dialog will appear and the analysis will halt.

Simulation Templates

SPICE simulators operate on a netlist and perform a standard set of simulations; AC, DC, TRAN, etc… By adding a script language, the results of these simulations can be automatically post processed - making available measurement results that correspond closely to real-world test measurements.

Analysis types most useful for design verification are:

- Sensitivity, including transient analysis
- Root Summed Square, RSS
- Extreme Value Analysis, EVA
- Worst Case by Sensitivity, WCS
- Standard simulation
- Monte Carlo
- Component Sweep
- Optimization

In theory, each of these analyses can be performed using ICL scripts; however, the scripts would have to be specialized for each circuit.

Simulation Templates were invented by Intusoft to integrate special ICL scripts with the netlist builder in order to create special analysis types. These address a class of problems associated with design verification for production and field compliancy. Simulation Templates control netlist options and mark insertion points for simulation control directives. These templates are easily edited by the user to optionally create custom report formats, and even to modify the analysis based on the user's special needs. Extensions to optimization, what-if, and sneak circuit analysis are possible.

Sensitivity Analysis

In this analysis, after running a reference simulation, each device parameter is perturbed and another analysis is run. For each measurement vector (i.e., Vout, iR3, etc.), the difference between the reference and the perturbed result (the sensitivity) is saved. This results in a number of simulations equal to the number of device parameters that have tolerances.

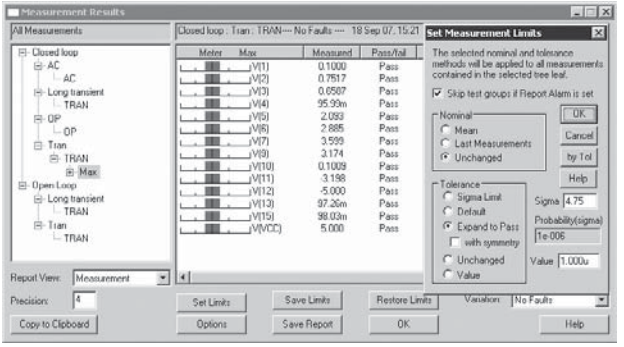
As a matter of convention, each tolerance is taken as the 3 sigma value, or 3 standard deviations. The Sensitivity results are reported as 3 sigma. The sensitivities for each parameter are reported for all measured vectors in descending order of magnitude in the IsSpice4 output file. The sensitivities can be tabulated for each measured vector or for each parameter.

RSS, Root Summed Square

In this analysis after running a reference simulation, each parameter is perturbed and another analysis is run. For each measurement vector, the difference between the reference and the perturbed result is saved. This results in a number of simulations equal to the number of parameters that have tolerances. Then, the square the sensitivities of each measurement are taken and are summed for each parameter. The square root of the result is saved in a plot called “rss.” Mathematically, the result for a single measurement is

Vresult = sqrt(Σ (Vresult(param) - Vresult(nominal))^2)

The RSS results are printed to the IsSpice4 output file in a format that can be read back in by SpiceNet. You can set the measurement test limits by expanding the measurements to “pass with symmetry” in the Results dialog, as shown.



If the result is linearly proportional to the change in the parameter value, then the RSS result is proportional to the standard deviation, which we could obtain from a statistical analysis. As a matter of convention, each tolerance is taken as the 3 sigma value, or 3 standard deviations, and we report the RSS results as 3 sigma. The parameter perturbation is set to 1 sigma, a compromise between a negligibly small value and the entire tolerance band. Making the perturbation fairly large eliminates some errors due to local maximum values occurring nearby. You can change this variation by editing the RSS Simulation Template.

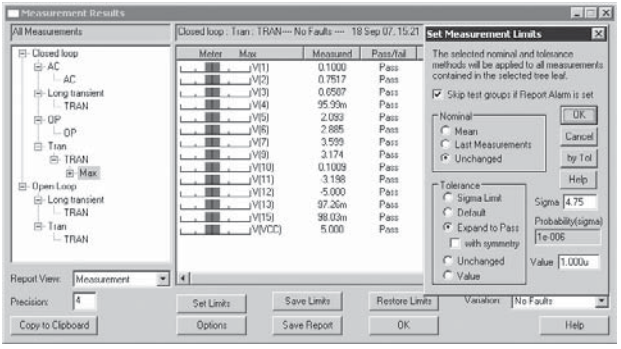
For many circuits, the variation of a measurement with respect to some parameters is highly nonlinear such that this analysis will give incorrect results. This frequently results in reporting smaller measurement variations than would be found using a statistical analysis.

When performing an AC analysis, it is often assumed that the response at each frequency can be considered independently. However, this is a poor assumption because single frequency results have an ambiguity in phase. When the difference in phase between two simulations is taken, there can be dramatically different results if one analysis is in a different phase plane than the reference simulation. Because of this, it is necessary to phase

extend the vectors desired to measure. This makes the AC analysis similar to the transient one, requiring measurements that resolve to scalar values. The duality between frequency and time seen using the Fourier transform makes this obvious.

EVA, Extreme Value Analysis

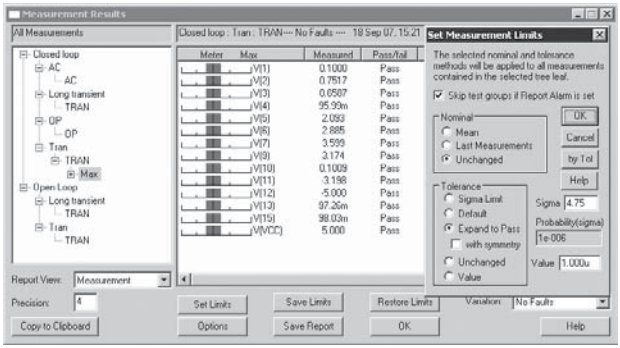
IIn this analysis, for each device containing toleranced parameter values, the parameters are varied to their extreme value so that scalar measurements (i.e., Vout, iR2, etc.) are maximized. The extreme value for each device tolerance with respect to a measurement is first based on the sign of a previously-run sensitivity analysis, whereby the device's tolerance is slightly perturbed. If the sensitivity analysis produced a positive change in measurement for a specified node or device, then the device under sensitivity analysis is railed to its maximum parametric value, or to its lowest value if a negative change was incurred at the measured node or device. This is the basis of the EVA-HI routine. The EVA-LO routine sets parameterized devices to their maximum or minimum value, based on which ever produced a minimized measurement result at a specified node or device during the sensitivity analysis. A simulation is then run using the new extreme parametric value for the toleranced device. The result for the node or device measurement is saved in the "evahi" plot, or "evalo" plot. The aforementioned sensitivity analysis and simulation are repeated for every parameterized device in the design, and for each measurement specified by the user. When all simulations are finished, the measurements are printed to the IsSpice4 output file in a format that can be read back in by SpiceNet for recording of measurements specified in Simulation Control's "Results" dialog. Additionally, the output file contains a summary report for the user's records. If making an evalo analysis is not opted, the user can set measurement min/max test limits by expanding the measurements to "pass with symmetry" (amongst other choices) in the "Results" dialog as shown below.



The extreme value in this analysis refers to the parameters, not the resultant measurements. **For most moderately complex circuits, the extreme value of the resultant measurement occurs when some of the parameters are at an intermediate value, rather than an extreme value.** However, we usually find that EVA results produce wider measurement test limits than Monte Carlo — making it a worthwhile investment. Finding the true extreme value of the resulting measurement requires a solution of a multi-parameter optimization problem. This becomes nearly impossible for larger circuits because the number of simulations grows by an amount equal to the product of parameters times the vectors. The EVA in its ICL script runs an analysis for each toleranced parameter to get perturbation results, then another for each measurement to get the final results.

WCS, Worst Case by Sensitivity

In this analysis a reference simulation is first run on the design and a plot of the data is stored to save the simulation results, notably at nodes or devices specified by the user (i.e., Vout, iR2, etc.). Then a new simulation is run for each device containing tolerance parameters, perturbing the parameter by a small fraction. The difference between these two sets of measurements are saved. The absolute value of operations performed on the difference measurements are summed (for the WCS_HI analysis) or subtracted (for the WCS_LO analysis), and saved in the IsSpice4 output file for viewing, and in a format that can be read back into the "Results" dialog accessed from SpiceNet's "Simulation Control" dialog (i.e., for viewing design "measurements"). This is not as rigorous as an EVA analysis or a worst case by optimization, however, it is the most computationally efficient method. In summary, differences in electrical measurements of interest between the reference simulation and sensitivity simulations, are continuously summed in a positive (WCS-HI), or negative (WCS-LO) direction to give a final measurement reading at any design node device specified by the user. You can set the min-max measurement test limits for prescribed nodes or devices across the design by expanding the measurements to "pass with symmetry" (amongst other choices) in Simulation Control's "Results" dialog; as shown below.



The WCS analysis is based on the assumption that each measurement is a linear function of all of the parameters. However, for most moderately complex circuits, this assumption is invalid. Generally you will get tolerances larger than the 3 sigma limits of a statistical analysis. Therefore, you should run a Monte Carlo analysis for at least 6 cases, then set tolerances based on the Monte Carlo analysis, usually to 5 sigma, before expanding the WCS data. In this way, you can be better assured that non-linear relationships are taken into account.

STD, Standard

This analysis variation, on the standard simulation, eliminates unnecessary vectors from scripted measurements. It also illustrates several of the template directives so you can use this as an example to begin writing your own Simulation Templates.

MONTE, Monte Carlo Analysis

Before performing this analysis, you must first set appropriate tolerance values on instance and model parameters using the part properties dialog for each part, or class of parts. Then you need to select the number of lots and cases to run from the <Monte Dialog>. Mak sure the Monte template is selected,

and the radio button above the question mark is selected. The Data reduction (right side) should be set to Interactive, and the Script checkbox must be checked. Then, Select one of the appropriate Test Configurations and press Simulate Selections. Progress will be shown in the IsSpice output window.

You can define the measurement results you want to view either before or after running the analysis. Measurements defined before running the analysis will be recorded in the database, and can be viewed using the <Results> button in the Simulation Control dialog. The measurements are set up for 5-sigma high values. Use the Set Limits dialog if you are establishing measurement tolerances. The usual procedure is to leave the nominal unchanged, and choose "expand to pass with symmetry" to setup a symmetrical tolerance band based on Monte Carlo results.

A new dialog in IntuScope can be activated after running a Monte Carlo analysis by pressing the <Monte> button in the <Add Waveforms> dialog. To plot the statistical results, you must have saved measurements in the "prob" plot (located in the Add Waveform dialog's "Type" box). You can easily add to the ones there by pressing the Monte Carlo box. Select vectors and functions from this dialog (individual boxes), then press the <Add Function to Plot> box just below. Incidentally, you can plot all cases of opposed vectors on X and Y axes, by first selecting desired vector's for both x and y axes in the Add Waveform dialog, then press the Add box. This will plot the first instance. Then, in the Monte dialog, press the Plot All Cases box for other instances.

What's also useful is when you select a measurement from the "prob" plot (Add Waveform dialog), and press either of the Plot boxes (Monte dialog). Histograms or cumulative probability plots result, scaled to your data set. Cumulative probability warps the x axis into "sigmas," based on a normal distribution. These plots help visualize the statistical distribution. Probability plots best fit a straight line through data points. If the data is normally distributed, it will lay along this straight line. The slope of the line, or first polynomial coefficient, is an estimate of the standard deviation. The rms error is shown, and if small compared to the standard deviation, you are most likely looking at a normal distribution.

Next, there is a feature to isolate the data set that created each data point. Simply place cursor 0 on a data point and press the report button. It tells you which simulation produced the data and shows each parameter's value and its sigma deviation. Using this feature, you can get an approximate separation of class members for cases that have bi-modal distributions. Then, you can separate class members into several groups for more detailed investigation.

> Note: *To place cursor 0 exactly on a data point, place it to the left of the point and with a blank accumulator, press the "0->Y" button in the Cursor control toolbar. The cursor will advance to the next data point each time you press the button. Using the "Y<-0" marches the cursor backward along data points.*

Finally, you can substitute the values associated with one of the simulations back into the schematic, to evaluate a "worst case" condition, or re-center the design.

OPTIMIZE, Multi-parameter optimization

Before performing this analysis, you must select the parameters to vary using the Tolerance/Sweep/Optimize tap in the parts properties dialog. The values entered for the optimize tolerance are similar to the ones used for Monte Carlo. The set represents a range of values for which optimization is constrained. For best results, there should be a minimum somewhere within the selected range. The values you select won't be retrievable after saving your document. Next, you must create an objective function. To do this, use the simulation control (ICAPS) dialogs measurement tab. You should have only one measurement in the test configuration. It doesn't matter what it's named. Then make sure the correct optimize template is selected, and the radio button above the question mark is selected. The Data reduction should be set to Interactive and the Script checkbox must be checked only if you have scripted measurements. Select one of the desired Test Configurations and press Simulate Selections. Progress will be shown in the IsSpice output window.

Optimization is performed using algorithms that minimize (achieve) your design objective function. Your two main challenges are to ask the "right" question through the objective function, and to bracket the solution space with the "tolerance" placed on the parameter that can vary. Three designs (Circuits\Snubber\Snubber.dwg, Circuits\ sprobe\sprobe.dwg and Circuits\Power\FwdTemplate\FwdTemplate.dwg) all have objective functions that can be used for optimization.

The optimization process consists of measuring the design objective function for a set of parameter values, then finding the parameter value that minimizes (achieves) the objective function. The Optimize.scp is a single pass version and Optimize2.scp is a 2-pass version. If you are doing single parameter optimization to select a component value, then optimize should work. If you are doing multi-parameter optimization, use optimize2. You can load either of these into IsEd5 and modify them. "Constants.maxiter" changes the number of iterations. The algorithm uses polynomial regression to make a high order curve fit so that it is possible to find a minimum value in the presence of local minimum values. The pure mathematical versions usually perform more iterations; but, a single iteration usually converges to within the component tolerance value, making further passes unnecessary.

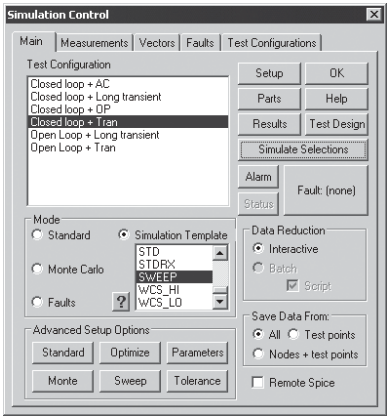
Sweep, Parameter Sweeping

In this analysis, you can linearly sweep an outer and optionally inner variable in a nested loop. You can assign a sweep variable to any device parameter and if you assign the same sweep variable to multiple parameters then their values will be changed together as a group. For example if you assign both R1 and R2 value parameter the same sweep variable Rvary then both parts will change their value at the same time for each step. The sweep dialog shows all defined sweep variables and their current available state. In the Tolerance/Sweep/Optimize tab we have the ability to activate/disable individual sweep variables to quickly change which parameter in a part we are sweeping.

Using the Simulation Control dialog's Sweep button. Fill in the Start, Stop and Step fields using numbers recognized by SPICE (i.e., 1u, 5m, …). The "name" field should be assigned the same name you assigned for the sweep variables in the part properties dialog. As with the Monte Carlo template, you can make

measurements before and/or after running a simulation.

Next, select the Sweep template as shown below, and the radio button above the question mark is selected. Directly above this in the Test Configuration box, highlight a desired selection. Data reduction (lower right corner) should be set to Interactive, and the Script checkbox must be checked. Now press Simulate



After the simulation has finished, you can use IntuScope to view the data. The Sweep button will be shown in the Add Waveforms dialog. Internally, a plot called sweep was made to hold the sweep results. If you didn't specify measurements before running the sweep template, you can plot data from the sweep plot using either the Add Waveforms dialog or the Sweep dialog.

Three special vectors were created; sweepdef (default), ramp and outer. Sweepdef is a sawtooth plot, which is the inner vector that repeats for each outer point. Outer is a staircase that steps up for each inner point. Ramp is a vector that goes from 0 to the product of (inner * outer - 1) points. Plotting a parameter versus ramp, and then plotting the family (i.e., outer vs. inner), you can check the link box in the scaling dialog and drag cursor 1 along the plot with ramp in the x-axis and view the parametric value in the outer vs. default (inner) plot.

Element Syntax

IsSpice4 Syntax Notation

IsSpice4 also accepts statements from the Interactive Command Language described in Chapter 11.

Format: R*name N1 N2 value*

Examples: R1 1 2 1KOHM
QLONGNAME 15 BASE 0 QN2222

Format statements similar to the one above are used throughout this chapter to define IsSpice4 netlist syntax.

Items in capital letters must appear exactly as shown.

- For example, the “R” in Rname.

Items in italics must be replaced by user-defined data.

- For example, the node numbers *“N1”* and *“N2”*, and the value of the resistor, *value*.

The description and examples will further clarify the required data.

Square brackets identify optional fields. When either one option OR another is required, the optional fields are separated by the word “or”.

For example: V*name N+ N-* [[DC] *value*]
+ [AC ma*gval* [*phaseval*]]
+ [PULSE *v1 v2* [*td* [*tr* [*tf* [*pw* [*per*]]]]]]
or [SIN *vo va* [*freq* [*td* [*kd*]]]]

In the voltage source statement, any combination of the three options, DC value, [[DC] *value*], AC value, [AC ma*gval* [*phaseval*]], or any one of the transient signal generators, (PULSE, SIN, PWL , etc.), can be selected. If a DC value is entered, the DC keyword is optional. Note that the DC keyword is nested inside the *value* parameter field, indicating that it is optional. For transient signal generators, the “or” indicates that only one of the options may be used.

Resistors/Semiconductor Resistors

Format: R*name N1 N2* [*value*] or [*Expr*]
[*M*=*value*] *[modname* L=*length* [W=*width*]]
[TEMP=*t*]

Examples: R1 1 2 1K
RS 15 32 r= 1K+1K∗sqrt(time) + 5∗temp
RMOD 3 7 RMODEL L=10u W=1u

Resistors can have expressions [Expr] for their value. See the Analog Behavioral Modeling Section for more information.

The resistor name must start with the letter R. *N1* and *N2* are the element nodes. The resistance value may be positive or negative, but not zero. Behavioral expressions may be used. M is the multiplicity factor that simulates parallel resistors.

The *modname* field refers to a resistor .MODEL statement. The information contained in the model statement is used for modeling temperature effects and for the calculation of the resistance value from geometric and process information. If *value* is specified, it overrides the geometric information and defines the resistance. If *an expression* or *value* is not specified, then the *modname* and *length* must be specified. If *width* is not

specified, then it will be taken from the DEFW value. The optional TEMP value is the temperature at which this particular resistor operates. It overrides the default temperature specification that is set by the .OPTIONS TEMP parameter.

The parameters available in the resistor model are:

Resistor Model Parameters

Name	Parameter	Units	Default	Example
TC1	1st order temperature coeff.	1/deg.C	0.0	-
TC2	2nd order temperature coeff.	1/deg.C^2	0.0	-
RSH	sheet resistance	Ω /sq.	-	50
DEFW	default width	meters	10e-6	2e-6
NARROW	narrowing due to side etching	meters	0.0	1e-7
TNOM	parameter measurement temp.	deg. C	27	50

Example: Resistor model with *modname*=RMOD

.Model RMOD R RSH=5 DEFW=100

See the .Model statement for more information.

The sheet resistance is used with the narrowing parameter NARROW and L and W from the resistor line to determine the nominal resistance by the formula:

$$R - RSH\frac{L - NARROW}{W - NARROW}$$

DEFW, in the resistor .model statement, is used to supply a default value for W if one is not specified on the device line. If either RSH or L is not specified, then the standard default resistance value of 1k is used. After the nominal resistance is calculated, it is adjusted for temperature by the formula:

In IsSpice4, temperature coefficients are specified using a resistor .MODEL statement.

$$R(T) = R(TNOM) * (1 + TC1 * \Delta T + TC2 * \Delta T2)$$

where ΔT = T - Tnom and Tnom = Nominal temperature, 27deg.C by default. Tnom can be changed using the .OPTIONS statement. T is the analysis temperature set by the TEMP parameter in the .OPTIONS statement.

See the .OPTIONS statement or the ICL Set command for more information on changing the circuit temperature.

To add temperature coefficients to a resistor

- Specify the resistor with a model name and a nominal value, for example;

  R1 1 0 1K RMOD

- Construct a .MODEL statement with temperature coefficients, for example;

  .MODEL RMOD R (TC1=.01 TC2=1E-6)

The model type of resistor is designated by the R in the .MODEL statement.

SPICE 2 Note: The method of specifying temperature coefficients in a resistor .MODEL statement is different than the syntax used in Berkeley SPICE 2.

Capacitors/Semiconductor Capacitors

UIC must be present in the .TRAN line for the IC= parameter to be used as an initial condition.

Capacitors can have expressions [Expr] for their value. See the Analog Behavioral Modeling section for more information.

Format: C*name N+ N-* [*value*] or [*Expr*]
[M=value] [*modname* L=*length* [W=*width*]] [IC=*v*]

Example:
```
CLOAD 5  0 10UF
CMOD  3  7  CMODEL  L=10u  W=1u
C1   8 0  .01UF  IC=10V; cap with initial voltage
Cin  2  0  C =1u+1P*FREQ^2; frequency dependent cap
CT 1 0 C={Cval}*(1+{TC1}*(TEMP)+{TC2}*(TEMP)^2)
; temperature dependent cap where {} are passed
 parameters or stated explicitly
```

N+ and *N-* are the positive and negative nodes. The capacitance value can be negative or positive, but not zero. The node polarity is used to reference an optional initial condition in the transient analysis. It is assigned using IC=*v* to make the initial voltage across the capacitor, V(N+) - V(N-), equal to *v*. M is the multiplicity factor that simulates parallel capacitors.

The *modname* value refers to a capacitor .MODEL statement. The information contained in the model statement is used for

the calculation of the capacitance value from geometric and process information. If *value* is specified, it overrides the geometric information and defines the capacitance. If *expression* or *value* is not specified, then the *modname* and *length* must be specified. If *width* is not specified, it will be taken from the DEFW value (10µm). Either *value* or *modname*, *length*, and *width* may be specified, but not both.

The parameters available in the capacitor model are:

Capacitor Model Parameters

Name	Parameter	Units	Default	Example
CJ	junction bottom capacitance	F/meters^2	0	5e-5
CJSW	junction sidewall capacitance	F/meters	0	2e-11
DEFW	default device width	meters	10e-6	2e-6
NARROW	narrowing due to side etching	meters	0.0	1e-7

See the .Model statement for more information.

Example: Capacitor model with *modname*=CMOD

.Model CMOD C CJ=2NF CJSW=1PF DEFW=2U

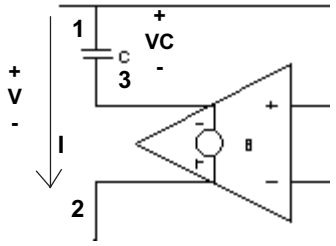
The capacitor has a capacitance computed as:

CAP = CJ ∗ (Length - Narrow) ∗ (Width - Narrow) + 2 ∗ CJSW ∗ (Length + Width - 2 Narrow)

Capacitors and inductors do not have a noise model.

Polynomial Capacitors

The polynomial capacitor function in other IsSpice programs and SPICE 2 is not included in IsSpice. The SPICE 2 polynomial capacitance can be represented with the following subcircuit:



The circuit is described by the following equations:

$$V = VC - B(V)$$
$$B(V) = Q0 + Q1*V + Q2*V^2 + ...$$
$$d(VC) = I/C\ dt = d(V + E(V))$$
$$C(V) = C*[1 + Q1 + 2*Q2*V + 3*Q3*V^2 + ...]$$
$$= P0 + P1*V + P2*V^2$$

Where P0, ... Pj are the polynomials that will be used in the capacitor POLY description and Q0,... Qj are used in the B element. For example, the SPICE 2 capacitor description,

C 1 2 POLY Value P0 P1 P2... **is replaced by:**
XC 1 2 POLYC {P0=val1 P1=val2 P2=val3...}

The polynomial capacitor equivalent circuit is built into the following subcircuit.

The polynomial capacitor that is created with this subcircuit works for the AC, DC, and Transient analysis types.

```
.SUBCKT POLYC 1 2
C 1 3 {P0}
B 2 3 v=v(1,2)^2*{P1/(2*P0)} + v(1,2)^3*{P2/(3*P0)}
+ v(1,2)^4*{P3/(4*P0)} ...
.ENDS
```

To use the subcircuit, replace the expressions in curly braces with the proper values, which are taken from the standard polynomial coefficients.

Note: a capacitor whose capacitance is dependent on voltage, or another circuit quantity, can be more easily created with the behavioral expressions capability. For example, a polynomial capacitor could be described as:

```
c1  2 0 C = P0 + P1*V(3) + P2*V(3)^2+ ...
```

where P0, P1..., are replaced with the polynomial coefficients and V(3) is the controlling voltage.

Inductors

Format: L*name N+ N- value* or [*Expr*] [IC=*i*] [M=value]

Example:
L5 5 3 10UHY
L1 8 0 .01HY IC=10MA
a) LiF 2 0 L = v(3) > 1 ? 0.1U : 1U
b) Lf 1 2 L= 1n + sqrt(Freq)
c) Lm 1 0 L = 1U+2*V(3) + I(R1)
d) Lt 2 0 l=0.1p + 1m*temp + 10u*temp^2

See the Analog Behavioral Modeling section for more information on the expressions capabilities.

The inductor name must start with the letter L. *N+* and *N-* are the positive and negative nodes. *Value* can be negative or positive, but not zero. Inductors can have an expression for the inductance value. For example: a) shows a If-Then-Else expression, If V(3) is greater than 1V then LiF=0.1μH, otherwise LIF=1μH.
b) describes a frequency dependent inductor. Note that the Freq value is zero during the transient analysis, hence the addition of 1n to the square root term. c) describes a voltage and current dependent inductor, while d) describes a temperature dependent inductor. All of these forms may be used for capacitors and resistors as well.

Current flow is considered to have a positive magnitude when it flows into the plus node of a IsSpice4 element.

Current flows from the positive node, through the inductor, to the negative node. Polarity is used to reference initial conditions. Initial conditions for the transient analysis are assigned using the IC= value to make the initial current equal to *i*. The UIC keyword must be present in the .TRAN statement for the IC to be used at the start of the transient analysis.

M is the multiplicity factor that simulates parallel inductors.

Polynomial inductors can be created with the behavioral expressions feature in IsSpice4. For example, a polynomial inductor could be described as:

L1 2 0 L = P0 + P1*I(V1) + P2*I(V1)^2+ ...

where P0, P1..., are replaced with the polynomial coefficients and I(V1) is the controlling current.

Coupled Inductors

Coupled inductors may need a small nonzero initial condition, on the L line, in order to aid the DC operating point and the start of a transient simulation.

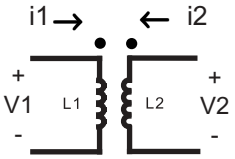
Format: K*name1* L*name2* L*name3* *value*

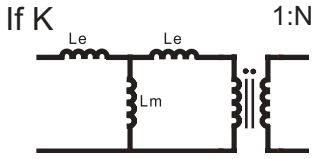
Example: K12 L1 L2 .9999

The coupling element name begins with K. Two inductors are referenced in the statement. The standard dot convention determines the polarity. The positive inductor nodes (first node in the L statement) carry the dot. Current flowing into a dot will flow out of the other dot, or voltage seen across one inductor will be reflected to the other inductor with the dots having the same voltage polarity. The coupling coefficient, *value*, must be less than 1 and greater than 0.

Coupled inductors are governed by the following behavior.

A IsSpice4 transformer; its equivalent circuit and related equations





$$M = K\sqrt{L1 * L2}$$

$$V1 = L1\frac{di1}{dt} + M\frac{di2}{dt}$$

$$V2 = M\frac{di1}{dt} + L2\frac{di2}{dt}$$

If $K \to 1$

$$L1 = Lm$$

$$L2 = N^2 L1$$

$$K = 1 - \frac{Le}{Lm}$$

The equivalent circuit, using discrete leakage and magnetizing inductances and an ideal transformer, is shown to the right.

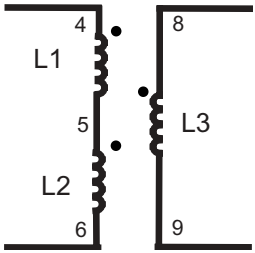
If multiple inductors are coupled, all combinations of coupling must be specified. Multiple winding transformers can be simulated in this manner.

Multiple coupled inductors must include all combinations of coupling.

For example:

```
L1  4  5  1UH
L2  5  6  2UH
L3  8  9  3UH
K12  L1  L2  .999
K23  L2  L3  .95
K13  L1  L3  .995
```

Represents:



Ideal Transmission Lines

Format: T*name N1 N2 N3 N4* Z0=*value*
+ [TD=*val2*] or [F=*freq* [NL=*nlen*]]
+ [IC=*v1, i1, v2, i2*]

Example:
```
T1  1  0  2  0  Z0=50  TD=25NS
T2  1  2  3  0  Z0=75  F=100MEG
```

Transmission line names must begin with the letter T. *N1* and *N2* are the nodes at port 1. *N3* and *N4* are the nodes at port 2. The transmission line length must be specified either in terms of delay time, or frequency and wavelength. Z0 specifies the characteristic impedance and TD specifies the time for a wave to propagate from port 1 to port 2. The optional specification of transmission line length using F and NL can replace the TD specification. F is a frequency and NL is the normalized electrical length of the transmission line with respect to the wavelength in the line at frequency F. If NL is omitted, it defaults to .25, a quarter wavelength. One of the two forms for expressing the line length must be specified.

See the .OPTIONS Minbreak for more information on reducing the simulation runtime when using ideal transmission lines.

Either port of the transmission line may be left unconnected in order to study the effects of open-circuited transmission lines. An unconnected dummy node number can be used to fill the syntax requirements, but both ports must still have a DC path to ground. The optional initial condition specification consists of the voltage and current at each of the transmission line ports. The initial conditions (if any) apply only if the UIC option is specified on the .TRAN line.

The ideal T-line is a bidirectional delay line. It models only one propagating mode. If all four nodes are distinct in the actual circuit, then two modes may be excited. To simulate such a situation, two transmission-line elements are required.

Note: Use of the lossy transmission line with zero loss (R=0, G=0) may be more accurate than the lossless transmission line, due to its superior implementation.

Lossy Transmission Lines

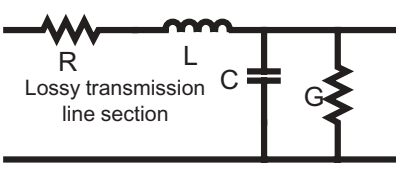
For a typical propagation delay of 125ps/inch, if Z is the impedance of the transmission line, then L=Z∗125p C=125p/Z Z=impedance and LEN is the length, in inches.

Format: O*name N1 N2 N3 N4 modname*

Example: O23 1 0 2 0 LOSSYMOD
Oconnect 10 5 20 5 Interconnect

The lossy transmission line begins with the letter O. *N1* and *N2* are the nodes at port 1; *N3* and *N4* are the nodes at port 2.

The O element uses the two-port LTRA model and can represent single conductor lossy transmission lines. It models a uniform distributed RLCG transmission line. The RC case may also be modeled using the URC model. However, the LTRA model is usually faster and more accurate. The operation of the LTRA model is based on the convolution of the transmission line's impulse responses with its inputs [reference 10-11].



The LTRA model takes a number of parameters, some of which must be provided, and some that are optional. The Resistance and conductance terms can have expressions for their values.

Example: 2.6kM of 26AWG Twisted Pair wire: R and G vary with frequency:

```
.Model PE4MM LTRA L=680U C=45N LEN=2.6
+ R=268.0 ∗ ABS((1 + FREQ / 1.3922E6)^0.493)
+G=2.4E-10 ∗ ABS((1 + FREQ / 5.2137)^0.87)
```

Lossy Transmission Line Model Parameters

Name	Parameter	Units/type	Default	Example
R	resistance/length	Ω/length	0.0	0.2
L	inductance/length	henrys/len	0.0	9.13e-9
G	conductance/length	mhos/len	0.0	0.0
C	capacitance/length	farads/len	0.0	3.65e-12
LEN	length of line	any length	none	1.0
REL	breakpoint control	none	1	0.5
ABS	breakpoint control	none	1	5
NOSTEPLIMIT	don't limit timestep to less than the line delay	flag	not set	nosteplimit
NOCONTROL	don't do complex timestep control	flag	not set	nocontrol
LININTERP	use linear interpolation	flag	not set	lininterp
MIXEDINTERP	use linear when quadratic seems bad	flag	not set	set
QUADINTERP	use quadratic interpolation	flag	set	quadinterp
COMPACTREL	special reltol for history compaction	none	RELTOL	1.0e-3
COMPACTABS	special abstol for history compaction	none	ABSTOL	1.0e-9
TRUNCNR	use Newton-Raphson method for timestep control	flag	not set	truncnr
TRUNCDONTCUT	don't limit timestep to keep impulse response errors low	flag	not set	-

The R and G parameters can have expressions for their values. See the Analog Behavioral Modeling Section for more info.

Example: 24 inch lossy line with L=9.13nH/inch, C=3.65pF/inch, and R=.2Ω/inch:

.Model Lline Ltra rel=1 r=.2 g=0 l=9.13e-9 c=3.65e-12 len=24 compactrel=1.0e-3 compactabs=1.0E-14

Example: lossless line L=9.13nH/inch and C=3.65pF/inch:

.Model Lfive Ltra rel=10 r=0 g=0 l=9.13e-9 c=3.65e-12 len=.2 steplimit quadinterp nocontrol

The following types of lines are implemented in IsSpice4:

RLCG (uniform transmission line with resistive and conductance losses), RC (uniform RC line), LC (lossless transmission line), and RG (distributed series resistance and parallel conductance only).

Parameter Explanation

The values of R, L, G, and C are specified per unit length, where LEN is the length of the line. LEN must be specified. For example, if LEN is .5 and R is specified in 1Ω/cm, then the line will be 1/2 cm long and have .5Ω resistance.

REL and ABS are quantities that control the setting of breakpoints. The option that is most effective for increasing simulation speed is REL. The default value of 1 is usually safe from the viewpoint of accuracy, but occasionally increases computation time. A value of greater than 2 eliminates all breakpoints, and may be worth trying depending on the nature of the rest of the circuit. However, keep in mind that it might not be safe from the viewpoint of accuracy. Breakpoints may usually be eliminated or reduced if it is expected that the circuit will not display sharp discontinuities. Values between 0 and 1 are usually not required, but may be used for setting many breakpoints.

NOSTEPLIMIT is a flag that removes the default restriction of limiting timesteps to less than the line delay in the RLC case. STEPLIMIT (default) forces the timestep to be limited to .8 times the delay of the transmission line.

NOCONTROL is a flag that prevents the default limiting of the timestep, based on convolution error criteria in the RLC and RC cases. This speeds up simulation but may reduce the accuracy of results in some cases.

TRUNCDONTCUT is a flag that removes the default cutting of the timestep to limit errors in the actual calculation of impulse response-related quantities.

NOCONTROL, TRUNCDONTCUT and NOSTEPLIMIT tend to increase speed at the expense of accuracy.

LININTERP is a flag that, when specified, will use linear interpolation instead of the default quadratic interpolation (QUADINTERP) for calculating delayed signals.

MIXEDINTERP is a flag that, when specified, causes IsSpice4 to judge whether or not quadratic interpolation is applicable. If it is not, IsSpice4 uses linear interpolation; otherwise it uses the default quadratic interpolation.

COMPACTREL and COMPACTABS are quantities that control the compaction of the past history of values stored for convolution. The legal range is between 0 and 1. Larger values of these parameters will lower the accuracy, but will usually increase simulation speed. These parameters are to be used with the TRYTOCOMPACT option, described in the .OPTIONS section. If TRYTOCOMPACT is not specified in the .OPTIONS statement, history compaction is not attempted and the accuracy is high.

TRUNCNR is a flag that turns on the use of Newton-Raphson iterations to determine an appropriate timestep in the timestep control routines. The default is a trial-and-error procedure, which cuts the previous timestep in half.

Multiple Coupled Lossy Lines

A utility program, called “Multidec”, is included in the MISC-PR subdirectory. Multidec produces SPICE compatible subcircuit representations of multiconductor coupled lossy transmission lines in terms of uncoupled (single) simple lossy lines. A batch file and a readme file are also included, and explain the operation of the program in detail.

Generic Model for Microstrip Style Interconnect

Geometric Values:
2μm thick (hth), 11μm wide (wth), 1m long (lth), and 10μm (d) above the ground.
(Note: Subcircuit parameters are shown in parentheses.)
Material:
aluminum - resistivity (sigma) = 2.74e-8- Ω m
Constants: (MKS units)
SiO2 dielectric, (er) =3.7 er0 = 8.85p , μ0 = 4e-7 * p, speed of light in free space = v0 = 1/sqrt(μ0 * er0) = 2.9986e8

Line parameter calculations (per meter):
Capacitance: parallel plate
C = er ∗ er0 ∗ Area1 / d = 3.7 ∗ 8.85p ∗ 11µ ∗ 1 / 10µ
= 36.02e-12 F/m + 30% (for fringing effects) = 46.8 pF/m

C_freespace = C0 = C/er = 46.8p/3.7 = 12.65 pF/m
v0 = 2.9986e8 = 1/sqrt(L∗C0) => L = 1/(C0 ∗ $v0^2$)
L = 1/(12.65p ∗ 8.9916e16) = 0.8792 µH/m
R = sigma ∗ lth / Area2 = 2.74e-8 ∗ 1 / (11µ ∗ 2µ)
= 1245.45 Ω/m

For microstrip lines that are very wide (w-> ×) the line will behave like a parallel plate capacitor. Equations in the { }'s perform the line parameter calculations for any set of geometric values.

Resulting Transmission line parameters:
Nominal z0 = sqrt(L/C) = 137/ , td = sqrt(LC) = 6.4ns/m

```
XLINE 2 0 3 0 LLINEG {SIGMA=2.74E-8 D=10U ER=3.7
+ ER0=8.85P LTH=1 WTH=11U HTH=2U LEN=.16}
∗ 16cm line length

.SUBCKT LLINEG 1 3 {ER0=8.85P}
O1 1 0 3 0 LOSSY
.MODEL LOSSY LTRA rel=1.8 len={LEN}m
+ r={SIGMA∗LTH/(WTH∗HTH)}ohms/m g=0
+ l={1/(1.3∗ER0∗(LTH∗WTH)/D∗(2.9986E8^2))}H/m
+ c={1.3∗ER∗ER0∗(LTH∗WTH)/D}F/m
.ENDS
```

Uniformly Distributed RC/RD Transmission Lines

Format: U*name N1 N2 N3 modname* L=*len* [N=*lumps*]

Example:
```
U1  1  2  0  URCMOD  L=50U
URC2  1  12  2  UMODL  l=1MIL  N=6
```

The uniformly distributed lossy RC line begins with the letter U. *N1* and *N2* are the two element nodes for the RC line. *N3* is the capacitance node. *Modname* is the lossy RC line's model name. *Len* is the length of the RC line in meters. *Lumps*, if specified, is the number of lumped segments used to model the RC line.

The URC model is derived from a model that was proposed by L. Gertzberrg in 1974. The model is created by using a subcircuit type expansion of the URC line into a network of lumped RC segments with internally generated nodes. The RC segments are in a geometric progression, increasing toward the middle of the URC line, with K as a proportionality constant. The number of lumped segments used, N, if not specified on the URC line, is determined by the following formula:

$$N = \frac{\log\left[F_{\max}\frac{R}{L}\frac{C}{L}2\pi L^2\left(\frac{K-1}{K}\right)\right]}{\log K}$$

RC/RD Transmission Line Model Parameters

Name	Parameter	Units	Default	Example
K	propagation constant	-	1.5	1.2
FMAX	maximum frequency of interest	Hz	1.0G	6.5Meg
RPERL	resistance per unit length	Ω/m	1000	10
CPERL	capacitance per unit length	F/m	1e-12	10pF
ISPERL	saturation current per unit length	A/m	0	-
RSPERL	diode resistance per unit length	Ω/m	0	-

Example: RC model with *modname*=TLINE

```
.Model TLINE URC K=1 FMAX=100MEG RPERL=1
+ CPREL=10PF
```

The URC line will be comprised of resistor and capacitor segments unless the ISPERL parameter is given a nonzero value. In this case, the capacitors are replaced with reverse-biased diodes with a zero-bias junction capacitance that is equivalent to the capacitance replaced, a saturation current of ISPERL amps per meter of transmission line, and an optional series resistance that is equal to RSPERL ohms per meter.

Switches (with Hysteresis)

Format: S*name N+ N- NC+ NC- modname* [ON] [OFF]
Format: W*name N+ N- vname modname* [ON] [OFF]

IsSpice4 contains 4 types of switches, S element (switch with hysteresis), B element switches, subcircuit switches, and a smooth transition switch (see next section).

Example:
```
S1  1  2  3  4  switch1  ON
s2  5  6  3  0  SM2  off
SWITCH1  1  2  10  0  Smodel1
w1  1  2  VCLOCK  Switch
W2  3  0  VRAMP  SM1  ON
wreset  5  6  Vclock  Lossysw  OFF
```

The voltage-controlled switch begins with the letter S. The current-controlled switch begins with the letter W. *N*+ and *N*- represent the connections to the switch terminals. The model name, *modname*, is mandatory, while the initial conditions are optional. For the voltage-controlled switch, nodes *NC*+ and *NC*- are the positive and negative controlling nodes, respectively. For the current-controlled switch, the controlling current is the current through the specified voltage source. The direction of the positive controlling current flow is from the plus node, through the named voltage source, to the negative node. ON or OFF options specify the switch state for the DC operating point.

The S/W element switches is equivalent to the Berkeley SPICE 3 switch.

The switch model allows an almost ideal switch to be described in IsSpice4. The switch is not quite ideal, in that the resistance can not change from 0 to infinity, but must always have a finite positive value. By proper selection of the on and off resistances, they can be effectively zero and infinity in comparison to other circuit elements.

The switch has hysteresis as described by the VH and IH parameters. For example, the voltage-controlled switch will be in the on state, with a resistance RON, at VT+VH. The switch will be in the off state, with a resistance ROFF, at VT-VH. The same applies for the current-controlled switch with IT and IH.

**See the description of the .OPTIONS GMIN parameter. Its default value results in an off resistance of 1.0E+12Ω.*

Switch Model Parameters				
Name	**Parameter**	**Units**	**Default**	**Switch**
VT	threshold voltage	Volts	0.0	S
VH	hysteresis voltage	Volts	0.0	S
IT	threshold current	Amps	0.0	W
IH	hysteresis current	Amps	0.0	W
RON	on resistance	Ω	1.0	both
ROFF	off resistance	Ω	1/GMIN	*both

Example: Voltage-controlled Switch *modname*=SMOD, on resistance=1μΩ, off resistance=1kΩ, on/off voltage=2V

```
.Model SMOD SW RON=1U ROFF=1K VT=2V
```

Example: Voltage-controlled Switch *modname*=SMOD, default resistances, on voltage=5V, off voltage=3V

```
.Model SMOD SW VT=4V VH=1V
```

Using a range of RON to ROFF of greater than 1E+12Ω is not recommended.

Example: Current-controlled Switch *modname*=CSMOD, on resistance 100Ω, off resistance 1MegΩ, on/off current 3mA

```
.Model SMOD CSW RON=100 ROFF=1MEG IT=3M
```

The use of an ideal element that is highly nonlinear, such as a switch, can cause large discontinuities to occur in the circuit node voltages. The rapid voltage change associated with a switch changing state can cause numerical roundoff or tolerance problems, which lead to erroneous results or timestep difficulties. You can improve the situation even further by taking the following steps:

Set the switch impedances only high and low enough to be negligible with respect to other elements in the circuit. Using switch impedances that are close to "ideal" under all circumstances will aggravate the discontinuity problem. Of course, when modeling real devices such as MOSFETS, the on resistance should be adjusted to a realistic level, depending on the size of the device being modeled.

If a wide range of ON to OFF resistance must be used (ROFF/RON >1E+12), then the tolerance on errors allowed during the transient analysis should be decreased by specifying the .OPTIONS TRTOL parameter to be less than the default value of 7.0. When switches are placed around capacitors, the .OPTIONS CHGTOL parameters should also be reduced. Suggested values for these two options are 1.0 and 1E-16, respectively. These changes inform IsSpice4 to be more careful near the switch points so that no errors are made due to the rapid change in the circuit response.

There are two other ways to model a switching function, both of which have the added advantage of a smoother transition region between the on and off states. The first uses a subcircuit approach with a dependent source, and the second uses the analog behavioral B element with in-line equations. The following subcircuits are stored in the Device.Lib library file.

Generic Switch Subcircuit

The generic switch is actually a voltage-controlled resistor. It can, therefore, be used as a switch or a potentiometer. The switch is created with a voltage-controlled current source (G element) that is tied back onto itself. The netlist is shown next.

The switch is a voltage-controlled resistor.

```
*OPEN WHEN V(3) = 0,
*CLOSED WHEN V(3) < > 0
*ON RESISTANCE = 1 / V(3)
*OFF RESISTANCE IS 1E12
.SUBCKT SWITCH 1 2 3
R1 1 2 1E12
G1 1 2 POLY(2) 1 2 3 0 0 0 0 0 1
.ENDS
```

The switch is very simple to use. Applying zero volts to the control input (node 3) opens the switch. The open resistance is 1E12 ohms = R1. It may be changed if desired. Applying any voltage to the switch control input, node 3, closes the switch and gives it a resistance of 1/V(3). For example, applying a voltage pulse 0 to 1 volt to the control input will change the resistance of port 1 to port 2 from 1E12 to 1 ohm. This switch model does not have any hysteresis.

Switch (Smooth Transition)

Format: A*name N+ N- NC+ NC- modname*

Example: A1 1 2 3 4 Switch
.Model Switch Vswitch

The smooth transition switch is equivalent to the built-in Pspice® switch.

IsSpice4 includes a special voltage-controlled switch with a smooth on-off transition region. This is in contrast to the Berkeley SPICE switch that has hysteresis. *N+* and *N-* represent the connections to the switch terminals. The model name, *modname*, is mandatory. *NC+* and *NC-* are the positive and negative controlling nodes, respectively.

Smooth Transition Switches
The Berkeley SPICE switch in IsSpice4 changes resistance rapidly when the threshold (VT+VH or VT-VH) is reached. As stated earlier, this may cause convergence problems. Therefore, this switch, which has a continuously changing resistance between the on and off voltage thresholds, can be substitued.

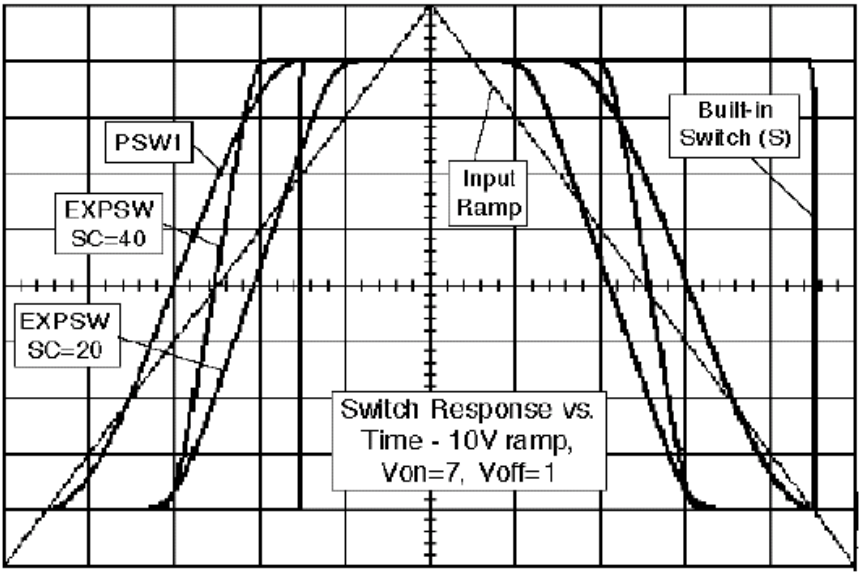
The smooth transition switch is C Code Model; hence its keyletter is an "A".

Switch Model Parameters

Name	Parameter	Units	Default
VON	ON voltage	Volts	1.0
VOFF	OFF voltage	Volts	0.0
RON	ON resistance	Ω	1.0
ROFF	OFF resistance	Ω	1.0E6

Example: .Model SMOD VSWITCH RON=1U VON=2V

Smooth Transition (B element) Switches
Shown next are generic models for several switches whose resistance changes gradually between the on and off voltage thresholds. Since the models are implemented with a single B element, they run very quickly. However, they are still not as fast as the built-in switches. The PSW1 switch emulates the code model switch outlined above while the second switch



uses an exponential transition region function. The subcircuit connections are the same as for the S and W switches: Out+ (1), Out- (2), Vctrl+ (3), Vctrl- (4). A graph of the different switch responses is shown above.

A variety of smooth transition switches using B element are available in under Switches in the Parts Browser dialog.

Smooth Transition switch, Von > Voff Case

```
.SUBCKT PSW1 1 2 3 4 {RON=1 ROFF=1MEG VON=1 VOFF=0}
*If VC > VON then RS=RON, If VC < VOFF then RS=ROFF,
* else RS 1MEG
B1 1 2 I=V(3,4) < {VOFF} ? V(1,2)/{ROFF} : V(3,4) > {VON} ?
+ V(1,2)/{RON} : V(1,2)/ (EXP(LN({(RON*ROFF)^.5}) +
+ (3 * LN({RON/ROFF}) * (V(3,4) - {(VON+VOFF)/2}) /
+ {2 * (VON-VOFF)}) - (2 * LN({RON/ROFF}) *
+ (V(3,4) - {(VON+VOFF)/2})^3 / {(VON-VOFF)^3} )))
.ENDS
```

The parameter SC can be varied to change the transition slope.

Fermi Probability Function

```
.SUBCKT EXPSW 1 2 3 4 {RON=1 ROFF=1MEG VON=1
+ VOFF=0 SC=20}
B1 1 2 I=V(1,2)/({RON} + ({ROFF-RON}/(1 + EXP({SC} *
+ (V(3,4)/{(VON+VOFF)/2} - 1)))) )
.ENDS
```

Independent Voltage Sources

Format:	V*name N+ N-*
Operating Point	+ [[DC] *value*]
AC/Noise analysis	+ [AC mag*val* [*phaseval*]]
Distortion analysis	+ [DISTOF1 [*F1magval* [*F1phaseval*]]]
	+ [DISTOF2 [*F2magval* [*F2phaseval*]]]
Transient analysis	+ v=expression
	+ [PULSE *v1 v2* [*td* [*tr* [*tf* [*pw* [*per* [*delay**]]]]]]]
	or [SIN *vo va* [*freq* [*td* [*kd* [*delay**]]]]]
	or [EXP *v1 v2* [*td1* [*t1* [*td2* [*t2*]]]]]
	or [PWL *t1 v1 t2 v2... tn vn*]
	or [SFFM *vo va freq* [*mdi* [*fs* [*delay**]]]]

In the DC field of the Voltage Source Properties Dialog enter v=expression. No affect on AC Analysis.

See the Alternating Current Stimulus section for more information on AC analysis stimulus requirements.

Example: DC operating point value=5V, transient 5V constant power supply. Note: The DC keyword is optional.

VCC 5 0 5V — VCC 5 0 DC 5V

Example: Current meter. Value for DC operating point, AC, and transient analysis is 0V. Impedance: 0 Ω .

VM1 2 3

Example: 5ns width pulse. Syntax follows the guidlines of B element expression syntax. Same as B element except no derivatives are calculated. The value of the source is calculated at each iteration using the previous sate of the simulator.

VIN 2 3 v = TIME < 5n ? 1 : 0

Example: Stimulus for the AC analysis. Used for frequency response and Bode plots. DC Operating point/transient analysis value, 0V.

VIN 1 0 AC 1

Example: Stimulus for the transient analysis only. Not to be used for AC/frequency response analysis. DC operating point value, 1V. Transient sinusoidal large signal waveforms with 1V offset and 5V peak value, 1MegHz frequency.

VIN 13 2 SIN 1 5 1MEG

Example: DC value 1V, AC magnitude 1, transient step from 0 at t0- to 1 at t0+, initial transient value is 0.

VIN 1 0 DC 1 AC 1 PULSE 0 1

Example: AC magnitude value=1, DISTOF1 magnitude=1 (default), DISTOF2 magnitude=.001.

```
VIN1 1 5 AC 1 DISTOF1 DISTOF2 0.001
```

Independent voltage source names begin with the letter V. *N+* and *N-* are the positive and negative nodes. Sources can be assigned values for the DC (operating point), AC, Noise, Distortion, and Transient analyses on the same line.

Current Flow

Positive current is assumed to flow into the positive node, through the source, and out the negative node. Initially, this may appear contrary to standard practice, but this convention is maintained for all IsSpice4 elements. Keep this fact in mind when measuring current flow with a voltage source.

DC (Operating Point) Value

The initial transient value overrides the DC value during the initial transient operating point.

The DC value is used for both the DC and transient analyses if no time-varying transient stimulus is specified. If the source value is time-invariant (e.g., a power supply), then the value may be preceded by the letters DC. Note, the DC sweep analysis (.DC) overrides this value. The DC value, if present, will be used as the operating point value for the AC analysis, while the initial transient source value will be used for the initial transient solution. If no DC value is given, the initial transient value will be used for the DC operating point.

AC/Noise Analysis Value

At least one source must have the AC keyword in order for the AC and Noise analyses to be performed.

Magval is the AC magnitude and *phaseval* is the AC phase, in degrees. The source is set to this value only during the AC and Noise analyses. The defaults for *magval* and *phaseval* are 1 and 0 degrees, respectively. The AC keyword must be present for the source to be used as a stimulus in the AC/Noise analyses. The AC parameter is used for the AC small signal frequency and noise analyses only, so its value will not be related to nonlinear or saturation characteristics. The AC magnitude value is usually set to 1 so that the node voltage data from the .PRINT AC statement is equal to the circuit gain (Gain = Voutput/Vin, which equals Voutput when Vin = 1).

At least one source must have the DISTOF1 and/ or DISTOF2 keywords for the distortion analysis to be performed.

Distortion Analysis Value
DISTOF1 and DISTOF2 are the keywords that specify the independent source distortion stimulus at the frequencies F1 and F2, respectively (See the description of the .DISTO statement). The keywords may be followed by optional magnitude and phase values. Like the AC values, the default values of the magnitude and phase for distortion stimulus are 1.0 and 0.0 degrees, respectively.

Note that voltage sources need not be grounded.

Measuring Current
Voltage sources can be used to measure current flow in a circuit branch. Voltage sources used solely as current meters have no value. The specification for reading the current through a voltage source during a particular analysis is determined by the .PRINT statement. As mentioned above, positive current flow in all IsSpice4 elements, including voltage sources, is from the positive node to the negative node. The orientation of the voltage source will, therefore, determine the polarity of the measured current.

To measure current in a circuit without affecting the circuit operation;

Voltage sources have a default value of zero for all analyses.

- Insert a zero-valued voltage source into the branch through that you would like to measure the current. For example, “VM1 1 2” will measure the current flowing from node 1 to node 2. “.PRINT TRAN I(VM1)” will save the value of the current through the source for the transient analysis.

The source will have no effect on the circuit operation since it represents a short circuit.

Alternating Current Stimulus
The inclusion of the proper circuit stimulus is important if you want the correct results from IsSpice4. One particular area that is commonly misunderstood is the difference between the “AC 1” AC/noise analysis stimulus and the “SIN” transient signal generator, explained in the next section. Although both provide a sinusoidal stimulus, they have vastly different uses. The AC 1 stimulus is used solely to produce a stimulus for the frequency

response analysis. The magnitude will not have a nonlinear effect on the reuslts because all of the device models are linearized before the frequency repsonse is performed. In contrast, the amplitude of the SIN wave stimulus can have a dramatic effect on the circuit operation during the transient analysis because nonlinear responses are included.

In summary:

- The AC1 keyword is used for the small-signal linear AC and noise analyses only. Use it if you want to obtain the frequency response, Bode plot output or circuit noise.

  VIN1 0 AC 1 - For AC Analysis

- The SIN stimulus is used for nonlinear transient analysis only. Use it if you want a large singal sinusoidal time-domain stimulus. The SIN stimulus does not have any effect during the AC analysis.

  VIN1 0 SIN 0 1 1kHz - For Transient Analysis

Transient Signal Generators

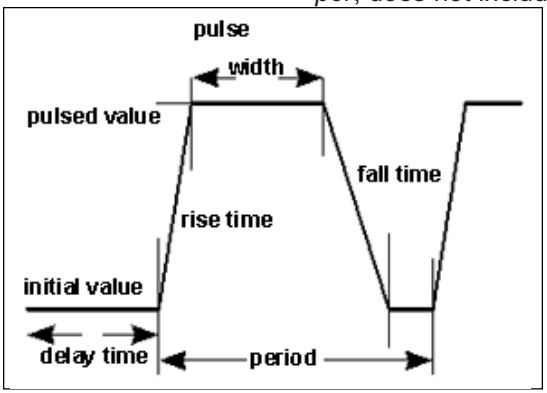
Note: Other Transient Signal Generators are available via the Parts Browser dialog under !Generators.

There are five independent transient signal functions: pulse, exponential, sinusoidal, piecewise linear, and single-frequency FM. The syntax for these generators can be specified together with stimuli for other analysis types ona singleindependent source line (See voltage source examples). However, only one of the transient signal generators (PULSE, SIN, EXP, PWL or SFFM) can be selected for each source.

Some of the parameters int he transient signal generators must be entered, while some of the parameters have defaults that are based on the TSTEP and TSTOP values. The values of TSTEP and TSTOP are defined in the .TRAN statement.

Format: **PULSE** *v2 v2 td tr tf pw per*

Generates a continuous periodic pulse train. The pulse period, *per*, does not include the initial delay, *td*.



Parameters		Units	Default
v1	Initial Value	Volts	None
v2	Pulsed Value	Volts	None
td	Delay Time	Sec	TSTEP
tr	Rise Time	Sec	TSTEP
tf	Fall Time	Volts	None
pw	Pulse Width	Sec	TSTOP
per	Period	Sec	TSTOP
delay	phase delay	degrees	0

For example, the waveform above was generated with:

V1 1 0 PULSE 0 1 100N 40N 90N 200N 390N

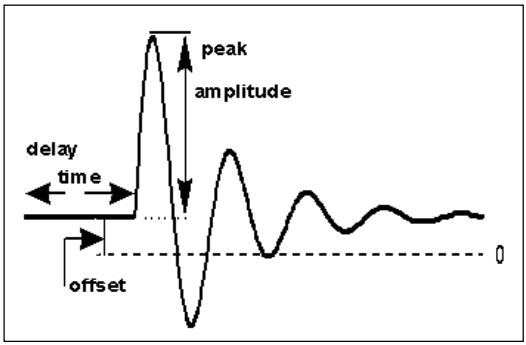
For example, a triangle wave:

V1 1 0 PULSE 0 1 0N 100N 100N 1P 200N

Format: **SIN** *vo va freq td kd*

Generates an optionally damped sine wave described by the following equations:

Time	Value
0 to TD	vo
TD to TSTOP	$v = vo + va * esp((td - t) * kd) * sin(2\pi f * (t - td))$



Parameters		Units	Default
vo	Offset	Volts	None
va	Peak Amplitude	Volts	None
freq	Frequency	Hz	1/TSTOP
td	DelayTime	Sec	0
kd	Damping coeff.	Sec^{-1}	None
delay	phase delay	degrees	0

SIN is used for time-domain analyses, not frequency-domain.

For example, the waveform above was generated with the following statement (0 to 1 volt, 10kHz, 50µs delay):

V1 1 0 SIN 0 1 10E3 50U 10E3

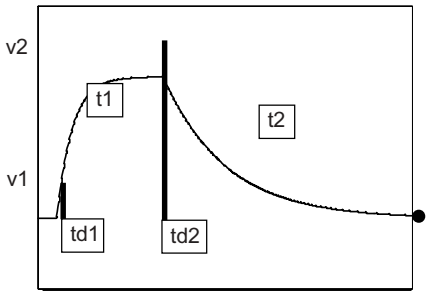
For example, a sine wave with an offset of 5 Volts, peak amplitude of 2 Volts, and a 1kHz frequency:

V1 1 0 SIN 5 2 1K

Format: EXP *v1 v2 td1 t1 td2 t2*

Generates an exponentially tapered pulse that is described by the following table:

Time	Value
0 to td1	$v1$
td1 to td2	$v1+(v2-v1)[1-e^{\frac{-(t-td1)}{t1}}]$
td2 to TSTOP	$v1+(v2-v1)\left[1-e^{\frac{-(t-td1)}{t1}}\right]+(v1-v2)\left[1-e^{\frac{-(t-td2)}{t2}}\right]$



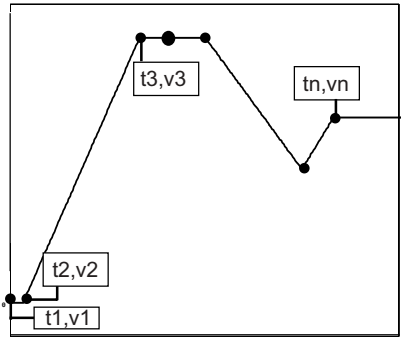
Parameters		Units	Default
v1	Initial Value	Volts	None
v2	Pulsed Value	Volts	None
td1	Rise Delay Time	Sec	0
t1	Rise Time Constant	Sec	TSTEP
td2	Fall Delay Time	Sec	td1 + TSTEP
t2	Fall Time Constant	Sec	TSTEP

Values with no default MUST BE SPECIFIED.

For example, the waveform to the left was generated with the following statement:

V2 3 0 EXP 0 1 30N 25N 200N 100N

Format: PWL *t1 v1 t2 v2 ..... tn vn*



A piecewise linear function is generated using straight lines between points. Each pair of values (tn, vn) specifies that the value of the source is vn (in Volts) at time = tn. The value of the source at intermediate values of time is determined by linear interpolation on the input values. The waveform value will remain at *vn* from *tn* to TSTOP.

For example, the waveform to the left was generated with the following statement:

See the "PWL Source" code model for a repeating PWL function.

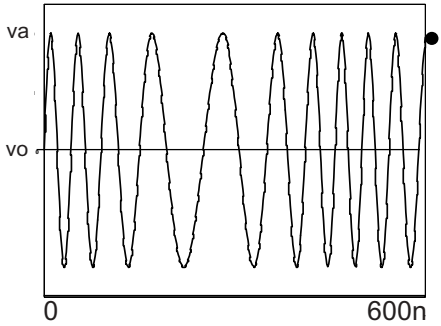
V1 2 0 PWL 0 0 10N 0 100N 1 150N 1 225N .5 250N .7

Note: Any number of continuation lines can be used to create long PWL waveform representations.

Format: SFFM *vo va fc mdi fs*

Generates a single frequency FM modulated signal described by the following equations.

value=vo + va * sine((2π*fc*time) + mdi * sine(2π*fs*time))



Parameter		Units	Default
vo	Offset	Volts	None
va	Amplitude	Volts	None
fc	Carrier frequency	Hz	1 / TSTOP
mdi	Modulation index		0
fs	Signal frequency	Hz	1 / TSTOP
delay	phase delay	degrees	0

For example, the waveform to the left was generated with the following statement:

V2 3 0 SFFM 0 1 16MEG 4 2MEG

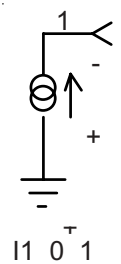
Independent Current Sources

Format:	I*name N+ N-*
Operating Point	+ [[DC] *value*]
AC/Noise analysis	+ [AC ma*gval* [*phaseval*]]
Distortion analysis	+ [DISTOF1 [*F1magval* [*F1phaseval*]]]
	+ [DISTOF2 [*F2magval* [*F2phaseval*]]]
Transient analysis	+ i=expression
	+ [PULSE *i1 i2* [*td* [*tr* [*tf* [*pw* [*per* [*delay**]]]]]]]
	or [SIN *io ia* [*freq* [*td* [*kd* [*delay**]]]]]
	or [EXP *i1 i2* [*td1* [*t1* [*td2* [*t2*]]]]]
	or [PWL *t1 i1 t2 i2... tn in*]
	or [SFFM *io ia freq* [*mdi* [*fs* [*delay**]]]]

Example:

```
IIN  1  0  DC  0  PULSE  0  1MA
IIN  1  0  i = TIME < 5n ? 1 : 0
ISRC  5  0  5MA
IIN 13 2   0.001  AC  1  SIN (0  1  1MEG)
ICARRIER 1 0 DISTOF1  0.1  -90.0
IMODULATOR 2 0 DISTOF2   0.01
```

Independent current source names begin with the letter I. *N+* and *N-* are the positive and negative nodes. Sources can be assigned values for the DC (operating point), AC, Noise, Distortion, and Transient analyses. The independent current source is very similar in syntax and function to the independent voltage source. For more examples and information on the transient current signal generators, see the syntax examples in the independent voltage source section.



Current Flow

Positive current is assumed to flow from the positive node, through the source, to the negative node. A current source of positive value will force current to flow into the *N+* node, through the source, and out of the *N-* node.

DC (Operating Point) Value

The DC value is used for both the DC and transient analyses if no time-varying transient stimulus is specified. If the source value is time-invariant (e.g., a stiff current source), then the value may optionally be preceded by the letters DC. Note the

DC sweep analysis (.DC) overrides this value. If the DC value is present, it will be used in the small signal bias solution that is calculated prior to the AC analysis. Otherwise, the initial transient value will be used for both the small signal bias solution and the initial transient solution.

AC Analysis Value

magval is the AC magnitude and *phaseval* is the AC phase, in degrees. The source is set to this value only during the AC and Noise analyses. The defaults for *magval* and *phaseval* are 1 and 0 degrees, respectively. Note, the AC keyword must be present for the source to be used as a stimulus in the AC and Noise analyses. If the source is not an AC small-signal input, the keyword AC should be omitted. The AC parameter is used for small-signal analysis so that its value is not related to saturation characteristics. The AC value is usually set to 1 so that the node voltage data from the .PRINT AC is equal to impedance (Impedance = Voutput/Iin = Voutput with Iin = 1).

At least one source must have the DISTOF1 and/ or DISTOF2 keywords in order to perform the distortion analysis.

Distortion Analysis Value

DISTOF1 and DISTOF2 are the keywords that specify that the independent source has distortion inputs at the frequencies F1 and F2, respectively (See the description of the .DISTO card). The keywords may be followed by optional magnitude and phase values. Like the AC values, the default values of the magnitude and phase for distortion stimuli are 1.0 and 0.0 degrees, respectively.

In the DC field of the Current Source Properties Dialog enter i=expression. Same as B element except no derivatives are calculated. No affect on AC Analysis.

Transient Analysis Value

Similar to the voltage source, there are five independent transient signal functions: pulse, exponential, sinusoidal, piecewise linear, and single-frequency FM. The syntax for these generators can be specified together with stimulus for the other analysis types on a single dependent source line (See voltage source examples). However, only one of the transient signal generators can be selected for each source. Some of the parameters in the transient signal generators must be entered, while some of the parameters have defaults that are based on the TSTEP and TSTOP values. The values of TSTEP and TSTOP are defined in the .TRAN statement.

Analog Behavioral Modeling

IsSpice4 is compatible with the SPICE 2 polynomial syntax.

The Analog Behavioral Model (ABM) capabilities in IsSpice4 give you the flexibility to describe electronic, mechanical, and physical processes in terms of transfer functions.

The ABM features of IsSpice4 are implemented using either linear dependent sources (keyletters E, F, G, or H) or the nonlinear dependent source (keyletter B).

SPICE 2 Syntax Note: the SPICE 2 syntax for E, F, G, and H elements, which provides nonlinear polynomial functions, is compatible with IsSpice4, but is not described here. This backward compatibility is made possible because IsSpice4 automatically converts the SPICE2 nonlinear polynomial syntax to the IsSpice4 nonlinear dependent source syntax that is used by the B element. Use of the B element is encouraged because its syntax is much more flexible.

Linear sources are useful for creating linear functions of voltage and current. The main features of the nonlinear dependent source include:

- Nonlinear functions of voltage/current where the functions can use trigonometric, transcendental, and algebraic operators, system variables, and node voltages and device currents in an equation-based format. The system variables include Time, Temperature, and Frequency.
- Boolean logic expressions, which are useful for simulating a variety of digital logic gates and functions.
- If-Then-Else expressions, which are useful for simulating digital logic gates, limiters, comparators, and switches.

Linear Dependent Sources

Note: in-line equations can not be used in linear sources; only in the nonlinear source.

IsSpice4 allows circuits to contain linear dependent sources, which are characterized by any of the four equations:

i = g ∗ v, v = e ∗ v, i = f ∗ i, and v = h ∗ i

where g, e, f, and h are constants representing transconductance, voltage gain, current gain, and transresistance, respectively.

Note: When using SPICE 2 polynomial syntax, avoid the use of “0.0” as a coefficient. Only “0” should be used.

Voltage-Controlled Voltage Sources

IsSpice4 does not require a resistor to be placed on the input to a voltage-controlled source, like SPICE 2, in order to satisfy the requirement of two connections at every node.

Format: E*name N+ N- NC+ NC- value*

Example: E1 3 4 2 1 1.5

The element name must start with the letter E. *N+* and *N-* are the positive and negative output nodes. *NC+* and *NC-* are the positive and negative controlling nodes. *Value* is the voltage gain. The input to the voltage-controlled source has an infinite impedance. It draws no current. The output voltage is computed as follows:

Vout= *value* * Vin,

where V(N+,N-)=Vout and V(NC+,NC-)=Vin.

Current-Controlled Current Sources

Format: F*name N+ N-* V*Name value*

Example: F1 3 4 VCC 2M

The element name must start with the letter F. *N+* and *N-* are

the positive and negative output nodes. Current flow is from the positive node to the negative node. *VName* is the voltage source whose current controls the output. *VName* must be the same as the voltage source's reference designation. *Value* is the current gain. The output current is computed as follows:

Iout = *value* * Iin

where I flowing from node N+ to N-=Iout and I(*VName*)=Iin.

Current-Controlled Voltage Sources

Initial conditions are not accepted on dependent sources. Use the .NODESET and .IC statements to establish initial values.

Format: H*name N+ N-* V*Name value*

Example: H1 3 4 VCC 2MΩ

The name must start with the letter H. *N+* and *N-* are the positive and negative output nodes. Current flow is from the positive node to the negative node. *VName* is the voltage source whose current controls the output. *VName* must be the same as the voltage source's reference designation. *Value* is the transresistance (in ohms). The output voltage is computed as follows: Vout = *value* * Iin

where V(N+,N-)=Vout and I(*VName*)=Iin.

Voltage-Controlled Current Sources

Format: G*name N+ N- NC+ NC- value*

Example: G1 2 3 5 0 10000UMHOS

The name must start with the letter G. *N+* and *N-* are the positive and negative output nodes. Current flows from the positive node to the negative node. *NC+* and *NC-* are the positive and negative controlling nodes. *Value* is the transconductance (in mhos). The output current is computed as follows:

Iout = *value* * Vin

where I flowing from node N+ to N-=Iout and V(NC+,NC-)=Vin.

Nonlinear Dependent Sources

Format: B*name* *N+* *N-* [I=*Expr*] [V=*Expr*]

Example:
```
B1 0 1 I=cos(v(1)+sin(v(2))
B21 0 V=ln(cos(log(v(1,2)^2)))-v(3)^4+v(2)^v(1)
B3 1 2 I=17
B4 out+ out- V=exp(pi^i(vdd))
```

The nonlinear source must begin with the letter B. *N+* and *N-* are the positive and negative nodes, respectively. The values of the V and I parameters determine the voltages and currents across and through the device, respectively. There is no distinction between current controlled and voltage-controlled sources for the B element. If I= is given, then the device's output is a current source. If V= is given, the device's output is a voltage source. One and only one of these parameters must be given.

AC Analysis Note: The small-signal AC behavior of the B source is a linear dependent source with a gain constant that is equal to the derivative(s) of the source at the DC operating point. (See the Behavioral Modeling Issues section)

In-line Equations, Expressions, And Functions

The B source allows an instantaneous transfer function to be written as a mathematical function using standard notation. The expressions, [*Expr*], can use algebraic, transcendental, or trigonometric functions, node voltages, device currents, and frequency, time, and temperature. The expressions can also be used on **resistors**, **capacitors**, **inductors**, and the R and G model parameters of the **lossy transmission line**. The output of the B source can be a voltage or current. The following section covers the B element syntax that you can use.

The following functions of real variables are defined:

Analog Behavioral Functions, Part 1

Function	Symbol/Description		Function	Symbol/Description	
abs(x)	|x|	absolute value	log(x)	log(x)	log base 10
acos(x)	$\cos^{-1}(x)$	result in radians	max(x,y)	Maximum of x and y	
acosh(x)	$\cosh^{-1}(x)$	result in radians	min(x,y)	Minimum of x and y	
asin(x)	$\sin^{-1}(x)$	result in radians	pwr(x,y)	$\|x\|^y$	
asinh(x)	$\sinh^{-1}(x)$	result in radians	pwrs(x,y)	$+\|x\|^y$ if x>0	$-\|x\|^y$ if x<0
atan(x)	$\tan^{-1}(x)$	result in radians	sin(x)	sin (x)	x in radians
atanh(x)	$\tanh^{-1}(x)$	result in radians	sinh(x)	sinh(x)	x in radians
atan2(y,x)	$\tan^{-1}(y/x)$	result in radians	sqrt(x)	$x^{1/2}$	square root
cos(x)	cos(x)	x in radians	sinh(x)	sinh(x)	x in radians
cosh(x)	cosh (x)	x in radians	sgn(x)	sgn(x)	signum, ± 1
exp(x)	e^x	exponential	stp(x)	1 if x>=0.0	0 if x<=0.0
expl(x,L)	e^x	e^x with limits	tan(x)	tan(x)	x in radians
ln(x)	ln(x)	log base *e*	tanh(x)	tanh(x)	x in radians

The analog behavioral functions, as shown in the Function column, can be used in any B element expression.

Real variables consist of numbers, voltages, device currents, and the key words “time”, “temp”, or “freq”. The following operations and constants are defined:

+ - * / ^ unary - e, pi

If the argument of log, ln, or sqrt becomes less than zero, the absolute value of the argument is used. If a divisor becomes zero or the argument of log or ln becomes zero, an error will result. Other problems may occur when the argument for a function in a partial derivative enters a region where that function is undefined.

Note: Do not use a plus sign (+) in front of positive numbers, for this will be interpreted as an addition operation.

Advanced Analog Behavioral Functions

Several more complex functions have been added for use in expressions. The operating point and transient behavior (Description field) and small signal behavior (AC, Noise, Distortion analyses) are summarized next.

Analog Behavioral Functions, Part 2

Function	Description	Small Signal Behavior
CEIL(x)	smallest integer not less than x or mag(x) if x is complex	linearized as $\frac{d}{dx}(x)CEIL(x)$
FLOOR(x)	largest integer not greater than x or mag(x) if x is complex	linearized as $\frac{d}{dx}(x)FLOOR(x)$
INT(x)	integer part of x or mag(x) if x is complex	linearized as $\frac{d}{dx}(x)INT(x)$
FRAC(x)	fractional part of x or mag(x) if x is complex	linearized as $\frac{d}{dx}(x)FRAC(x)$
MOD2(x)	floating-point remainder of x/2 or mag(x)/2 if x is complex	linearized as $\frac{d}{dx}(x)MOD2(x)$
SINC(x)	sin(x)/x	linearized as $\frac{d}{dx}(x)\frac{x\cos(x)-\sin(x)}{x^2}$
MAG(x) or M(x)	magnitude of x	linearized as $\frac{d}{dx}(x)$
PHS(x) or P(x)	phase of x in degrees	linearized as $\frac{d}{dx}(x)\frac{1}{x^2+1}$
REAL(x) or R(x)	**r**eal part of x	linearized as $\frac{d}{dx}(x)$
IMAG(x) or IMG(x)	imaginary part of x	linearized as 0, i.e. no AC value
RAND(x)	a random number between 0 and x is generated every time this function is called (i.e. every iteration)	linearized as 0, i.e. no AC value
RANDC(x)	same as RAND(x), except that the first random number generated will remain constant throughout the simulation	linearized as 0, i.e. no AC value

Random Numbers and Waveforms

The random numbers generated by the Rand and Randc functions use a uniform distribution. For random noise, use of the PWL C code model will provide superior results. The PWL code model allows standard PWL sequences to be repeated. The PWL points are taken from an external file. This makes stimulus data from other programs easily accessible. The PWL code model also produces random noise, but has been written so that it runs faster than the internal SPICE PWL source.

Additional Operators

A modulus operator can be used between any two variables and/or constants in an expression. Its functionality in transient and AC analysis is described below.

Operator	Description	AC Analysis
x % y	floating-point remainder of x/y or mag(x)/mag(y) if x and/or y are complex	linearized as $\left(\frac{d}{dx}(x)+\frac{d}{dx}(y)\right)(x\%y)$

Expression Examples using Different Functions

```
b1 3 0 v = phs(1.0e3 / (freq+1k))      ; frequency gain block
L1 2 0 v = v(1) * int(rand(5.25))      ; randomly varying inductor
r1 2 3 r = 1000+1000 * exp(V(3)) ; voltage-controlled resistor
b1 3 0 v = (3.5 * v(2)+2.25) % (1.25*v(2)+2.0)
b1 2 0 v = int(mod2(v(1)))
b2 3 0 v = frac(mod2(v(1)))
```

STP Function

The unit step function can be used to suppress a value until a given amount of time has passed. Ex, V(1)*STP(10ns-TIME) gives a value of 0.0 until 10ns has passed and then give a value of V(1).

Using branch currents in expressions

IsSpice4 expressions support two types of branch currents:

Currents through voltage source elements

a) Linear Independent Voltage Sources, V
b) Nonlinear dependent sources (with V=), B
c) Voltage-controlled Voltage Sources, E
d) Current Controlled Voltage Sources, H

Currents through non-voltage source elements

a) Capacitors, C
b) Current Controlled Current Sources, F
c) Current Controlled Switches, W
d) Diodes, D
e) Inductors, L
f) Resistors, R
g) Voltage-controlled Switches, S
h) Voltage-controlled Current Sources, G

Expression Examples using Currents

```
b3 5 0 v = 1p + (i(c1) / (freq * 1U))^2
b1 3 0 I = log(i(g1)) * exp(i(r1))
b1 2 0 v = i(d1)

c1 2 0 c = exp(v(1)) * i(c2)
r7 4 5 r = 1k + 1k * i(vin)
L2 5 0 L = 0.1u + 0.1m * i(r1)
```

Using Time, Frequency, and Temperature in Expressions

You can now specify simulation time, simulation frequency and/or circuit temperature as a variable in an expression. The keyword **TIME** specifies the instantaneous time, **FREQ** specifies the current AC analysis frequency, and **TEMP** specifies the temperature as listed in the .OPTIONS TEMP= value (default =27). The effects of these variables in transient and AC analysis are summarized below.

Variable	Description
TIME	Current simulator time in **seconds**, 0 in the AC analysis
FREQ	Current simulator frequency in **radians**, 0 in the Transient analysis
TEMP	Circuit temperature in **degrees C** as specified in the .OPTIONS statement; default = 27, same for both the AC and Transient analyses

Expression Examples using Temp, Time, and Freq

Note: Use Mag(Freq) when using FREQ in an If-Then-Else expression.

```
b1 3 4 I = 2.0 * v(1)^0.5 + 3.0*v(2)*time + v(2)*sqrt(temp)
b2 2 0 V = 6.283e3/(freq+6.283e3)
b1 1 0 V = time * V(10)

rt 1 2 r= 1.0e3 + 1.0e3 * sqrt(time) + 2.0 * log(temp)
R1 2 0 R=1 + 1K * int(TIME)

Lte 1 2 r= 10u + 1n * sqrt(mag(Freq)) * sqrt(temp)
c2 2 0 c =1u + 1p * sqrt(mag(Freq)) + 1.0e-6 * log(temp)
```

Time Subcircuit

To get time into an expression or represented as a node voltage for other purposes, you can also integrate the current from a constant current source with a capacitor and use the resulting voltage to represent time. Don't forget to set the initial voltage across the capacitor and use UIC in the .TRAN statement. For example, node Tvalue = time:

```
I1  0  Tvalue  1
C1  Tvalue  0  1  IC=0
R1 Tvalue 0 1E12
```

Behavioral Modeling Issues

Element Values

If you use current or voltage to control the value of a component, you need to be careful to first have a default value so if the controlling value is 0, then the component value will not be 0. For example,

R1 1 2 r = I(vin) * 100 should be
R1 1 2 r = 50 + I(vin) * 100

If R1 1 2 r = I(vin) * 100 is used and the current in VIN is zero, then the error message "R1 set to 1000" will be issued and the value of R1 will be set to 1K. Whenever the current in Vin becomes nonzero, then the value of R1 will change appropriately. The same goes for use of the time and freq variables. For the AC analysis, the output of b1, b1 1 0 V = time * V(10), is zero. A more appropriate usage might be b1 1 0 V = 1+ time * V(10)

Division

Be careful when performing division. Care should be taken to prevent the denominator from becoming zero, otherwise a non-convergence may result. For example, in B4 7 8 I=V(2) / V(4), if V(4) should become zero during the DC operating point or transient analysis, the circuit may fail to converge.

Exponential With Limits

Frequently, as in the above B element, an exponential function is required. In order to keep the value of the exponential from becoming too large and causing convergence problems, a special exponential function has been included in IsSpice4, EXPL. The format is EXPL(function,limit_value). For example: **B1 1 0 v= expl(v(3),50)** will produce an output voltage that is exponential until v(3)=50. Above 50, the output of the B element will become a straight line.

Branch Currents

IsSpice4 expressions support two types of branch currents: currents through voltage source elements, and currents through non-voltage source elements (shown previously). The main difference between these two groups is that the currents through voltage source elements are added as a circuit variable to the circuit equations, and are calculated along with the node voltages. However, the currents through non-voltage source elements are not added to the circuit equations as an independent variable, mainly to keep the matrix small, reduce memory usage, and reduce simulation time. For example, the current through a resistor at each iteration can easily be calculated from the corresponding node voltages and the resistance value. There is no need to add this current to the circuit equations as an independent variable.

The only restriction for performing a transient analysis is that if you want to use currents as variables, you must use current through a voltage source to achieve accurate results. If you use current through other elements, then you will get a warning that the results may be inaccurate.

You cannot perform an AC analysis on an expression containing circuit variables. Otherwise, unexpected results will be produced. AC analysis on expressions is made successful only when such expressions exclusively contain **FREQ**, **TIME**, **TEMP** or math functions - not circuit variables.

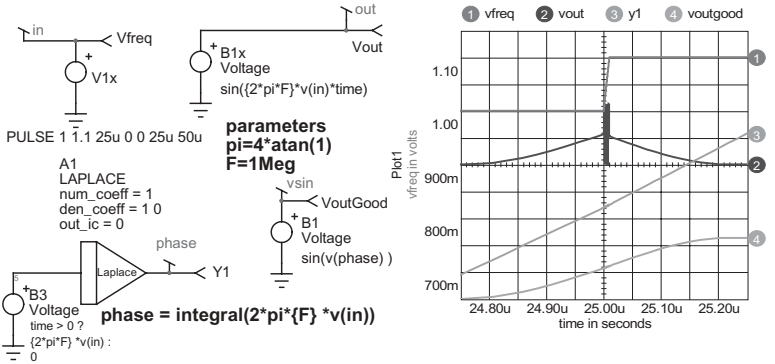
Voltage Controlled Oscillator

It's convenient to model an oscillator using a behavioral expression:

V = sin(2*pi*v(F)*time)

But, if v(F) is a variable, the interpretation is incorrect as shown below.

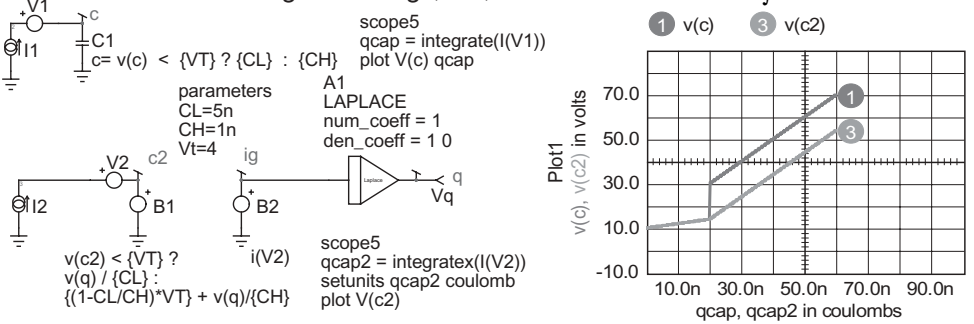
Note: A voltage controlled oscillator gives unexpected results if frequency is used as a variable instead of phase; phase continuity is required.



As the controlling voltage sweeps from 1 volt (1MegHz) to 1.1 volts (1.1MegHz), the resulting waveform at vout has high frequency oscillation. But that follows the equation exactly! What we really wanted was to define the output as the sine of phase. By doing that you get the correct interpretation shown as voutgood.

Voltage Variable Capacitor

In figure below, we want to make a capacitor change value at a particular voltage. That can model the behavior of a MOS transistor as its gate to drain voltage crosses threshold. The proper interpretation should use charge, not capacitance. When the capacitance value is changed, a voltage discontinuity occurs. If charge is controlled, the expected result is achieved, that is, **V = Q / C**. A similar argument can be made for making an inductor vary as a function of current. The integral of voltage, flux, needs to be used or $I = \int Vdt / L$.



Nonlinear Elements

In addition to the expressions feature, nonlinear capacitors, resistors, and inductors may be created with the B element. Nonlinear resistors are obvious. Nonlinear capacitors and inductors are implemented with their linear counterparts by a change of variables implemented with the nonlinear dependent source. The following subcircuit will implement a nonlinear capacitor:

```
.Subckt  Nonlinear cap  pos  neg
Bx 1 0 v=f(v(pos,neg)) ; calculate f(input voltage)
Cx 2 0 1 ; linear capacitance
*Vx: Ammeter to measure current into the capacitor
Vx 2 1 DC 0Volts
*Drive the current through Cx back into the circuits
Fx pos neg Vx 1
.Ends
```

For example, a sigmoidal capacitance characteristic could be described by the following:

```
.SUBCKT     MISD     1          2          3     {M=2 VT=3}
*                    Anode    Cathode    Charge Test Point
B2  4 0 V= V(1,2) *1/( 1 + exp^({M} * (V(2,1) + ({VT})))))
V1  4 3 0
C1  3 0 {CO}
F1  1 2 V1 1
.ENDS
```

Nonlinear inductors are similar. Several nonlinear resistor examples are shown in the Switches section.

Note: Nonlinear resistors, capacitors, and inductors can also be generated, in some cases more easily, by putting the expression directly on the element line. For example:

```
C1 3 0   C = {Co} * 1/( 1 + exp^({M} * (V(2,1) + ({VT})))
```

Boolean Logic Expressions

Format: B*name* *N+* *N-* [V=*Expr*]

The examples describe a 3-input Nand gate, an inverter, and a 2-input Or gate.

Example:
```
b1 4 0 v = ~(v(1) & v(2) & v(3))
B1 invout 0 v= ~v(2)
b1 3 4 v = v(1) | v(2)
```

The nonlinear dependent source element may be used to create models of digital logic functions. This is accomplished by including Boolean operators in the [*Expr*] function.

The expression [*Expr*] may consist of Boolean operators and any of the functions in the Analog Behavioral Functions section. There is virtually no limit to the length or complexity of the expressions that can be used. The following operations are defined for the Boolean logic options:

& - And | - Or ~ - Not

.OPTIONS parameters control the default logic levels.

There are three .OPTIONS parameters that control the default threshold and logic 1/0 output levels. They are:

Lone	Value for logic one	default =3.5
Lzero	Value for logic zero	default=.3
Lthresh	Value for logic threshold	default=1.5

For example: .OPTIONS LONE=5 LZERO=0 LTHRESH=2.5 would reset the logic one level to 5V, logic zero to 0 volts, and the logic threshold to 2.5V.

The expression is evaluated at each internal time point and if the result is greater than the threshold (Lthresh), the output voltage is set to a logic one (Lone). If the result is less than the threshold, the output voltage is set to a logic zero (Lzero).

The derivative of a boolean function is taken as zero.

AC Analysis Note: The small-signal AC behavior of the Boolean expression is a linear dependent source, or sources, with a proportionality constant that is equal to the derivative (or derivatives) of the source at the DC operating point.

Caution: Digital Logic With Feedback
The Boolean logic expressions are ideal delay-free functions. When creating digital functions, you should keep this in mind and add realistic delays wherever possible. In circuits with feedback, it is almost always necessary to add a delay to each gate. Otherwise, the continuously evaluated Boolean expressions may not converge to a solution. Initial conditions may also be needed in order to properly initialize bistable circuits. The IC= keyword on the capacitor, the .IC command, and the UIC keyword in the .TRAN statement are used for this purpose. For example, see the following D Flip-Flop circuit.

To add delay to a gate, insert an RC combination to the output. This will give the gate some rise/fall time and delay. For example:

```
b1 4 0 v = v(1) & v(2)    2-Input And
r1  4 0 1                 RC Delay
c1 4 0 .87nF IC=0         IC = Optional Initial Condition
```

Note: If you set up a series of gates as subcircuits, you can use the parameter passing feature to pass initial conditions to the gate.

Example: Flip-Flop

```
DFLOP
.TRAN .25U 10U
*ALIAS  V(1)=VQ
*ALIAS  V(2)=VQN
.PRINT TRAN  V(1)  V(2)  V(3)  V(10)  V(12)
X4 1 7 6 2 NAND3 {IC=0}
X6 4 5 2 1 NAND3 {IC=1}
X7 8 7 12 3 NAND3 {IC=1}
X8 4 9 3 8 NAND3 {IC=0}
X9 10 7 2 9 NAND3 {IC=1}
X10 3 12 9 10 NAND3 {IC=0}
VCLK 12 0 3.5 PULSE 3.5 0 0 0 0 1U 2U
V6 7 0 PULSE 0 3.5
V4 4 0 3.5
```

```
*Flip-Flop CONTINUED
V7 3 5 -.25
V8 10 6 -.25
.subckt nand3 1 2 3 4
b1 44 0 v = ~(v(1)&v(2)&v(3))
r 4 44 1
c 4 0 100n IC={IC}
.ends
.end
```

Caution: Internal Time Step Aliasing
Digital gate models in IsSpice4 have a continuous output. This is different from the discontinuous output that is seen in logic simulators. The Boolean functions are evaluated on a continuous basis, but since they do not have any inherent capacitive delays, they do not contribute to IsSpice4's control of the time step. And, since the internal time step in IsSpice4 occurs at varying intervals, it may be necessary to clamp down on the timestep in order to see the exact time that a switching transition occurs.

To make sure the timestep does not get too large

- Include the TMAX parameter in the .TRAN statement.

It is difficult to give an estimate of what percentage of the TSTEP value the TMAX value should have. It will be different for different circuit topologies. However, setting the TMAX value from 1/10 to 1/2 of the TSTEP value will typically provide adequate resolution if enough data points are taken.

For example: Run the A-to-D circuit in the If-Then-Else section with and without the TMAX parameter.

If-Then-Else Expressions

Format:
B*name N+ N-* V=*EVALUATION* ? *OUTPUT_VALUE1* or *EXPRESSION* : *OUTPUT_VALUE2* or *EXPRESSION*

More Simply:
B*name N+ N-* V=if *EVALUATION* is true then v(N+,N-)=*OUTPUT_VALUE1* else v(N+,N-)=*OUTPUT_VALUE2*

> **Note:** Spaces should be included before and after the "?" and ":" symbols. Also, V= may be substituted with I=.
>
> The [*Expr*] field in the nonlinear dependent source element may be inserted with an If-Then-Else clause that has a wide variety of uses.
>
> *EVALUATION, OUTPUT_VALUE,* and *EXPRESSION* may consist of any combination of the functions or operators listed in the In-line Equations and Functions section or boolean operators. There is virtually no limit to the length or complexity of the expressions that can be used.
>
> The *EVALUATION* expression can use greater than ">" or less than "<" test. Equal is not allowed.
>
> Extended "If-then-else" expressions can also be used. For example:

B*name N+ N-* V=if *EVALUATION1* is true then if *EVALUATION2* is true v(N+,N-)=*OUTPUT_VALUE1* else v(N+,N-)=*OUTPUT_VALUE2*

B*name N+ N-*V=if *EVALUATION1* is true then v(N+,N-)=*OUTPUT_VALUE1* else if *EVALUATION2* is true v(N+,N-)=*OUTPUT_VALUE2:* else *OUTPUT_VALUE3*

> **AC Analysis Note:** The small-signal AC behavior of the nonlinear source is a linear dependent source (or sources) with a proportionality constant equal to the derivative (or derivatives)

of the source at the DC operating point. The If-then-else function does not have a derivative. However, the output expression or function selected by the If-then-else test is differentiated.

If-Then-Else Examples
3 input nand gate with user defined levels
b1 4 0 v=v(1) > 1.5 ? v(2) > 1.5 ? v(3) > 1.5 ? 0.3 : 3.5
If v(1) is greater than 1.5 then if v(2) is greater than 1.5 then if v(3) is greater than 1.5 then v(4)=0.3 else v(4)=3.5

Limiter
b1 2 0 v=v(1) < .5 ? v(1)∗.5 + .25 : v(1) > 1.53 ? 1.54 : v(1)
If v(1) is less than .5 then v(2)=v(1)∗.5+2.5 else if v(1) is greater than 1.53, then v(2)=1.54 else v(2)=v(1)

Comparator
b1 3 0 v=v(1,2) < 0 ? 5 : .1
If voltage difference v(1)-v(2) is less than 0, then v(3)=5V, else v(3)=.1V

Switch
b1 2 0 v=v(vctrl) < 0 ? v(3) : v(4)
If vctrl is less than 0, then v(2)=v(3), else v(2)=v(4)

Note: Use Mag(Freq) when using FREQ in an If-Then-Else expression.

If-Then-Else Examples Using Behavioral Modeling Functions
r1 3 5 r = abs(v(2)) > 0 ? abs(v(2)) : 1
rin 1 2 r = v(3,4) > 1 ? 1K ∗ (1+rand(2.0)) : 1K ∗ (1+rand(2.0))
L1 1 2 L = I(r1) > 1 ? 1K : 250 ∗ log(temp)
cin 2 0 c = abs(v(3)) > 1 ? 0.1U : 1U ∗ log(temp)

Example: A-D Converter Circuit
A to D converter test
vin 1 0 pulse 0 2 0 1u 0 1u
.tran 10n 1u 0 1n
x1 1 2 10 adc
x2 2 3 11 adc
x3 3 4 12 adc
x4 4 5 13 adc
x5 5 6 14 adc
x6 6 7 15 adc

```
x7 7 8 16 adc
x8 8 9 17 adc
.print tran v(10) v(11) v(12) v(13) v(14) v(15) v(16) v(17)
.print tran v(1) v(2) v(3) v(4) v(5) v(6) v(7) v(8)
.subckt adc in out bin
b1 bin 0 v= (v(in) > 1) ? 1 : 0
b2 out 0 v= 2 * (v(in) - v(bin))
.ends
.end
```

The A-to-D module consists of :

.subckt adc in out bin	<-	Input, Output, Binary level
b1 bin 0 v= (v(in) > 1) ? 1 : 0	<-	Test - if v(in) is greater than 1, then binary output bin=1, else bin=0
b2 out 0 v= 2*(v(in) - v(bin))	<-	Output of A-to-D subcircuit = 2 * (v(in)-v(bin))
.ends		

Device Models Statements

The model parameters associated with Code Models are described in the next chapter.

The passive elements described thus far typically require only a few parameter values. Even those devices that use a .MODEL statement (resistor, capacitor, lossy transmission line) can be defined with a simple set of parameters. However, code models and semiconductor devices included in IsSpice4 require many parameter values to describe their behavior. Often, the same device may be used in several places in the circuit. For these reasons, model parameters that describe a semiconductor are defined on a separate .MODEL line.

The use of a semiconductor, or code model requires two steps. First, each device must be called. The calling statement starts with the device's keyletter and reference designation name, then the nodes to which the device is connected, and finally the device's model name. The second step uses a .MODEL statement to define the parameters that describe the device. The model name is used to link the device call line with its respective .MODEL definition statement. This scheme alleviates the need to specify all of the model parameters on each device call line.

Other optional parameters may be specified on the calling line for some devices. These include geometric factors and initial conditions.

The area factor, available on some semiconductor call lines, determines the number of equivalent parallel devices of the specified model. Not all of the model parameters are affected. The affected parameters are marked under the heading 'area' in the following model parameter tables with either an asterisk, if the area multiplies the parameter value, or a / sign, if the area divides the parameter value. For the MOSFET call line, several geometric factors associated with the channel and the drain and source diffusions maybe specified.

Two different forms of initial conditions may be specified for some devices. The first form is included to improve the DC convergence for circuits that contain more than one stable state. If a device call line contains the OFF keyword, then the DC operating point is determined with the terminal voltages for that device set to zero. After convergence is obtained, the program continues iterating to obtain the exact value for the terminal voltages. If a circuit has more than one stable DC state, the OFF keyword can be used to force the solution to correspond to a desired state. If a device is specified OFF when the device is conducting, the program will still obtain the correct solution (assuming the solutions converge) but additional iterations will be required since the program must independently converge to two separate solutions. The .NODESET line serves a purpose similar to the OFF option. The .NODESET statement is easier to apply and is the preferred means to aid convergence, although it does require the specification of a voltage value, whereas the OFF keyword does not.

The second form of initial conditions are for use with the transient analysis. These are true 'initial conditions', as opposed to the convergence aids above. When issued along with the UIC keyword in the .TRAN statement, the IC= values will be used for the terminal voltages with which the transient analysis will start. See the description of the .IC line and the .TRAN line for a detailed explanation of initial conditions.

.Model Statement

Format: .MODEL *modname TYPE*(pn1=*pv1* pn2=*pv2*..)

Examples:
```
.MODEL MOD1 NPN (BF=50 IS=1E-13 VAF=50)
.MODEL CONNECT LTRA (R=0.2
+ L=9.13nC=3.65pF LEN=5 STEPLIMIT
+ REL=2 COMPACTREL=1.0e-4)
```

The .MODEL line specifies a set of model parameters that are referenced by one or more element statements. *Modname* is the model name used to connect the .MODEL statement to the calling element. Model names may begin with a number, but it is best to follow the SPICE 2 convention of beginning a model name with the same letter as the calling element (e.g. D for Diode, Q for BJT).

TYPE is one of the following types:

Type	Keyletter	Device
C	C	Capacitor
R	R	Resistor
CSW	W	Current-controlled switch
SW	S	Voltage-controlled switch
LTRA	O	Lossy RLCG transmission line
URC	U	Uniformly Distributed RC/RD T-line
D	D	Diode
NJF	J	N-channel JFET
PJF	J	P-channel JFET
NMOS	M	N-channel MOSFET
PMOS	M	P-channel MOSFET
NPN	Q	NPN BJT
PNP	Q	PNP BJT
NMF	Z	N-channel MESFET
PMF	Z	P-channel MESFET

Note: this list does not contain the code model 'types' that are described in the next chapter.

Parameter values are defined by appending the parameter name, as given with each model type, followed by an equal sign and the parameter value. Model parameters that are not given a value are assigned the default values.

The format used to call a device and define its behavior is:

General Format: Device Call Statement
.Model Definition Statement

Format: *Keylettername Node Numbers modelname*
.MODEL *modelname TYPE* (*parameters*)

For example, to call a diode, we would use the statement:

```
D1 1 0 DN4148
```

To define the D1 element, we would use the statement:

```
.MODEL DN4148 D(RS=.8 CJO=4PF IS=7E-09 N=2
+ VJ=.6V TT=6E-09 M=.45 BV=100V)
```

Notice how the model name DN4148 links the calling statement with the definition. Also, note that the model name does NOT define what kind of element the device is calling. For example, just because a Q1 element has a model name of 2N2222, that does not mean that the Q1 device is an NPN BJT. The *type* must say NPN. An element is defined by the *type* value and the model parameter values.

For some devices, the method of defining the type of device with the TYPE parameter is redundant. For example, the diode call above can only have one *type*, D. Any other *type* value will be considered an error. For a Q keyletter, however, either a PNP or an NPN *type* is acceptable. Once a keyletter is used to call a model name, the *type* must agree, otherwise, an error will result.

Diodes

Format: D*name NA NC modname* [*area*] [OFF] [IC=*vd*]
+ [TEMP=*t*] [M=value]

Examples:
```
DBRIDGE 2 10 DIODE1 OFF
DCLMP 3 7 DMOD 3 IC=0.2V TEMP=50
```

See the "Working with Model Libraries" book for the diode's equations.

Node *NA* is the anode and node *NC* is the cathode. *Modname* is the model name, *area* is the area factor (default 1.0), and OFF indicates an (optional) initial condition on the device for DC analysis. The (optional) initial condition specification using IC =*vd*, the voltage across the diode, is intended for use with the UIC option. It should be used when you desire a specific starting condition, other than the operating point value, at the beginning of the transient analysis. The (optional) TEMP value is the temperature at which this device is to operate, and overrides the temperature specification in the .OPTIONS statement. M is the multiplicity factor that simulates parallel devices.

Diode Model Parameters

Name	Parameter	Units	Default	Example	Area
IS	saturation current	A	1.0e-14	1.0e-14	*
RS	ohmic resistance	Ω	0	10	/
N	emission coefficient	-	1	1.0	
TT	transit-time	sec	0	0.1Ns	
CJO	zero-bias junction capacitance	F	0	2pF	*
VJ	junction potential	V	1	0.6	
M	grading coefficient	-	0.5	0.5	
EG	activation energy	eV	1.11	1.11 Si 0.69 Sbd 0.67 Ge	
XTI	saturation-current temp. exp.	-	3.0	3.0 jn 2.0 Sbd	
KF	flicker noise coefficient	-	0		
AF	flicker noise exponent	-	1		
FC	coefficient for forward-bias depletion capacitance formula	-	0.5		
BV	reverse breakdown voltage	V	∞	40.0	
IBV	current at breakdown voltage	A	1.0e-3		*
TNOM	parameter measurement temp.	deg C	27	50	
IBVL	lowlevel reverse breakdown knee current	A	0		
IKF	high-injection knee current	A	∞		
ISR	recombination current parameter	A	0		
NBV	reverse breakdown ideality factor	-	1		
NBVL	low-level reverse breakdown ideality factor	-	1		
NR	emission coefficient for isr	-	2		
TRS1	1st order RS temp coefficient	-	0		
TRS2	2nd order RS temp coefficient	-	0		
TBV1	1st order BV temp coefficient	-	0		
TBV2	2nd order BV temp coefficient	-	0		

Uses standard Berkley Diode model equations unless extra parameters in bold are used.

*The symbols * or /, in the area column, indicate whether the parameter is multiplied or divided by the area.*

The diode is modeled using an ohmic resistance in series with a diode. The DC characteristics of the diode are determined by the parameters IS, N and RS. Charge storage effects are modeled by a transit time, TT, and a nonlinear depletion layer capacitance, which are determined by the parameters CJO, VJ, and M . The temperature dependence of the saturation current is defined by the parameters EG, the energy gap, and XTI, the saturation current temperature exponent. Reverse breakdown is modeled by an exponential increase in the reverse diode current and is determined by the parameters BV and IBV (both are positive numbers).

Sample Models:

```
.MODEL DN4001 D (Is=5.86E-06 N=1.70 Bv=6.66E+01
+ IBV=.5u RS=36.2m Cjo=5.21E-11 Vj=.34 M=.38 TT=5.04u)
* 50 Volt  1.00 Amp  3.50 us  Si Rectifier  Diode  07-01-1990

.MODEL  DN753  D(RS=4.68  BV=6.10  CJO=346P TT=50N
+ M=.33  VJ=.75  IS=1E-11  N=1.27  IBV=20MA)
* 1N753, 6.2 Volt Zener Diode
```

Bipolar Junction Transistors

Format: Q*name NC NB NE* [*NS*] *modname* [*area*] [OFF]
+ [IC=*vbe,vce*] [TEMP=*t*] [M=value]

Examples:
```
Q23 10 24 13 QMOD IC=0.6,5.0
Q50A 11 26 4 20 MOD1
```

See the Working with Model Libraries book for BJT equations.

All transistor calls begin with the letter Q. *NC*, *NB*, and *NE* are the collector, base, and emitter nodes, respectively. *NS* is the (optional) substrate node. If unspecified, ground is used. *Modname* is the model name, *area* is the area factor, and OFF indicates an (optional) initial condition on the device for the DC analysis. If the area factor is omitted, a value of 1.0 is assumed. The symbols * or /, in the area column, indicate whether the parameter is multiplied or divided by the area. The (optional) initial condition specification, using IC =*vbe,vce,* is intended for

use with the UIC option on the .TRAN statement. It should be used when you desire a specific initial condition, other than the operating point value, at the beginning of the transient analysis. The (optional) TEMP value is the temperature at which this device is to operate, and overrides the temperature specification in the .OPTIONS statement.

M is the multiplicity factor that simulates parallel devices.

*The * or / symbols in the area column indicate whether the parameter is multiplied or divided by the area.*

The BJT Model

The bipolar junction transistor model in IsSpice4 is an adaptation of the integral charge control model of Gummel and Poon. This modified Gummel-Poon model extends the original model to include several effects at high bias levels. The model will automatically simplify to the Ebers-Moll model when certain parameters are not specified.

The BJT parameters used in the modified Gummel-Poon model are listed below. The parameter names used in earlier versions of SPICE are still accepted.

BJT Model Parameters

Name	Parameter	Units	Default	Example	Area
IS	transport saturation current	A	1e-16	1e-15	*
BF	ideal maximum forward beta	-	100	200	
NF	forward current emission coefficient	-	1.0	1.75	
VAF	forward Early voltage	V	∞	200	
IKF	corner for forward beta high current roll-off	A	∞	0.01	*
ISE	B-E leakage saturation current	A	0	1e-13	*
NE	B-E leakage emission coefficient	-	1.5	2	
BR	ideal maximum reverse beta	-	1	0.1	
NR	reverse current emission coefficient	-	1	1	
VAR	reverse Early voltage	V	∞	200	
IKR	corner for reverse beta high current roll-off coefficient	A	∞	0.01	*

BJT Model Parameters, *continued*

ISC	B-C leakage saturation current	A	0	1e-13	*
NC	B-C leakage emission	-	2	1.5	
RB	zero bias base resistance	Ω	0	100	/
IRB	current where base resistance falls halfway to its min value	A	∞	0.1	*
RBM	minimum base resistance at high currents	Ω	RB	10	/
RE	emitter resistance	Ω	0	1	/
RC	collector resistance	Ω	0	10	/
CJE	B-E zero-bias depletion capacitance	F	0	2pF	*
VJE	B-E built-in potential	V	0.75	0.6	
MJE	B-E junction exponential factor	-	0.33	0.5	
TF	ideal forward transit time	sec	0	0.1ns	
XTF	coefficient for bias dependence of TF	-	0		
VTF	voltage describing VBC dependence of TF	V	∞		
ITF	high-current parameter for effect on TF	A	0		*
PTF	excess phase at freq=1/(TF∗2π) Hz	degrees	0		
CJC	B-C zero-bias depletion capacitance	F	0	2pF	*
VJC	B-C built-in potential	V	0.75	0.5	
MJC	B-C junction exponential factor	-	0.33	0.5	
XCJC	fraction of B-C depletion capacitance connected to internal base node	-	1		
TR	ideal reverse transit time	sec	0	10nS	
CJS	zero-bias collector-substrate capacitance	F	0	2pF	*
VJS	substrate junction built-in potential	V	0.75		
MJS	substrate junction exponential factor	-	0	0.5	
XTB	forward and reverse beta temperature exponent	-	0		
EG	energy gap for temperature effect on IS	eV	1.11		

BJT Model Parameters, *continued*

XTI	temperature exponent for effect on IS	-	3	
KF	flicker-noise coefficient	-	0	
AF	flicker-noise exponent	-	1	
FC	coefficient for forward-bias depletion capacitance formula	-	0.5	
TNOM	parameter measurement temp.	°C	27	50
NK	High-Current Roll-Off Coefficient	-	0.5	

See the .IC line description for a better way to set transient initial conditions.

The DC response is defined by the parameters IS, BF, NF, ISE, IKF, and NE, which determine the forward current gain characteristics. The parameters IS, BR, NR, ISC, IKR, and NC determine the reverse current gain characteristics. VAF and VAR determine the output conductance for the forward and reverse regions. Three ohmic resistances RB, RC, and RE are available. RB can be current dependent using the IRB and RBM parameters. Base charge storage is modeled by forward and reverse transit times, TF and TR. The forward transit time TF can be bias dependent, using the XTF, VTF, and ITF parameters. Nonlinear depletion layer capacitances are determined by CJE, VJE, and MJE for the B-E junction, CJC, VJC, and MJC for the B-C junction and CJS, VJS, and MJS for the C-S junction. The temperature dependence of the saturation current, IS, is determined by the energy-gap, EG, and the saturation current temperature exponent, XTI. Additionally, base current temperature dependence is modeled by the beta temperature exponent, XTB.

```
.MODEL QN2222 NPN (IS=15.2F NF=1 BF=105 VAF=98.5
+ IKF=.5 ISE=8.2P NE=2 BR=4 NR=1 VAR=20 IKR=.225
+ RE=.373 RB=1.49 RC=.149 XTB=1.5 CJE=35.5P CJC=12.2P
+ TF=500P TR=85N)
* 30 Volt .8 Amp 300 MHz SiNPN Transistor

.MODEL QN2904 PNP (IS=381F NF=1 BF=51.5 VAF=113
+ IKF=.14 ISE=46.1P NE=2 BR=4 NR=1 VAR=20 IKR=.21
+ RE=.552 RB=2.21 RC=.221 XTB=1.5 CJE=15.6P CJC=20.8P
+ TF=636P TR=63.7N)
* 40 Volt .6 Amp 250 MHz SiPNP Transistor
```

Junction Field-Effect Transistors

Format: J*name ND NBG NS modname* [*area*] [OFF] [IC=*vds,vgs*] [TEMP=*t*]

Examples: J1 7 2 3 JM1 OFF

See the description of the .IC line for a better way to set initial conditions.

Calls to the JFET begin with the letter J. *ND*, *NG*, and *NS* are the drain, gate, and source nodes, respectively. *Modname* is the model name, *area* is the area factor, and OFF indicates an (optional) initial condition on the device for DC analysis. If the area factor is omitted, a value of 1.0 is assumed. The symbols * or / in the area column indicate whether the parameter is multiplied or divided by the area. The (optional) initial condition specification, using IC=*vds, vgs,* is intended for use with the UIC option on the .TRAN line. It should be used when you desire a specific starting condition, other than the operating point value, at the beginning of the transient analysis. The (optional) TEMP value is the temperature at which the device operates, and overrides the .OPTIONS TEMP value.

M is the multiplicity factor that simulates parallel devices.

JFET Models

See Working with Model Libraries book for the JFET equations.

There are two models associated with the JFET. The Berkeley JFET model is derived from the FET model of Shichman and Hodges. The DC characteristics are defined by the parameters VTO and BETA, which determine the variation of drain current with gate voltage. LAMBDA determines the output conductance and IS the saturation current of the two gate junctions. Two ohmic resistances, RD and RS, are included. Charge storage is modeled by nonlinear depletion layer capacitances for both gate junctions, which vary as the -1/2 power of junction voltage (M fixed at .5), and are defined by the parameters CGS, CGD, and PB. A new doping profile parameter, B, was added in SPICE 3F. The JFET can also emulate a GaAs MESFET depending on the parameters used. The Parker-Skellern model was developed by Macquarie University in Sydney Australia. It contains several new model parameters that provide greatly improved DC, AC, and transient performance. See ref. 10-1, 10-2, and 10-3.

JFET Model Parameters

Name	Parameter	Units	Default	Example	Area
Basic DC Parameters					
B	doping profile parameter**	-	1	1.1	
BETA	transconductance parameter	A/V^2	1e-4	1e-3	*
DELTA	coef of thermal current reduction*	1/W	0	5	/
IBD	breakdown current of diode junction*	A	0	1e-7	*
IS	gate junction saturation current	A	1e-14	1e-12	*
LAMBDA	channel length modulation parameter	1/V	0	0.05	
LFGAMMA	drain feedback parameter*	1/V	0	0.01	
MXI	saturation potential modulation*	-	0	0	
N	gate junction ideality factor*	-	1	1.5	
P	power law (triode region)*	-	2	2.4	
RD	drain ohmic resistance	Ω	0	2.5	/
RS	source ohmic resistance	Ω	0	2.5	/
VBD	breakdown potential of diode junction*	V	1	3	
VST	critical potential for subthreshold conduction*	V	0.025	0.12	
VTO	threshold voltage	V	-2.0	-2.5	
XI	velocity saturation index*	-	1e+3	0.3	
Z	exponent of velocity sat. formula*	-	2	2	
Charge Storage Parameters					
CGS	zero-bias G-S junction capacitance	F	0	5pF	*
CGD	zero-bias G-D junction capacitance	F	0	1pF	*
PB	gate junction potential	V	1	0.6	
FC	coefficient for forward-bias depletion capacitance formula	-	0.5		
XC	amount of cap. reduced at pinch-off* (used when CMOD=2)	-	0	0.2	
CMOD	select capacitance model to use* (1=Berkeley JFET, 2=Statz model)	-	1	2	

Frequency Dependent Parameters				
HFGAMMA	high freq. drain feedback parameter∗	1/V	0	0.08
TAU	drain feedback relaxation time∗	sec	0	0.001
TAUD	thermal relaxation time∗	sec	0	1e-6
Temperature/Noise Parameters				
TNOM	parameter measurement temperature	degC	27	50
KF	flicker noise coefficient	-	0	1e-15
AF	flicker noise exponent	-	1	1

∗∗ Berkeley SPICE 3F parameters, ∗ Parker-Sekellern MESFET parameters; Macquarie University, See references [10-1,2, and 3] for more information about the Macquarie MESFET model parameters.

```
.MODEL BF510 NJF (VTO=-.8 BETA=2.8M LAMBDA=15.5M
+ RD=4.04 RS=3.63 IS=11.8F PB=1 FC=.5 CGS=8.95P
+ CGD=995F)
∗ 20 Volt  30M Amp  28.8 ohm  Dep-Mode N-Channel J-FET
.MODEL J175 PJF (VTO=-4.90 BETA=3.6M LAMBDA=6.89M
+ RD=14 RS=14.6 IS=3.51F PB=1 FC=.5 CGS=12.5P
+ CGD=16.5P KF=5.3434E-16 AF=1)
∗ 45 Volt  20M Amp  100 ohm  Dep-Mode P-Channel J-FET
```

GaAs Field Effect Transistors - MESFETs

Format: *Zname ND NG NS modname area*] [OFF] [IC=*vds, vgs*] [M=value]

Examples: Z1 1 7 2 ZM1 OFF

See the Working with Model Libraries book for the MESFET equations.

Calls to the MESFET begin with the letter Z. *ND*, *NG*, and *NS* are the drain, gate, and source nodes, respectively. *Modname* is the model name, *area* is the area factor, and OFF indicates an (optional) initial condition on the device for DC analysis. If the area factor is omitted, a value of 1.0 is assumed. The symbols * or / in the area column indicate whether the parameter is multiplied or divided by the area. The (optional) initial condition specification, using IC=*vds, vgs,* is intended for use with the

UIC option on the .TRAN line. It should be used when you desire a specific initial condition, other than the operating point value, at the beginning of the transient analysis. See the description of the .IC line for a better way to set initial conditions.

M is the multiplicity factor that simulates parallel devices.

The MESFET Models
IsSpice4 contains several MESFET models, each differentiated by the Level parameter.

LEVEL = 1 -> Statz Model, reference [10-10], Default Level
LEVEL = 2 -> Anadigics Corp. “NICE” MESFET Model
LEVEL = 3 -> HEMT Model, Maquarie University [10-13, 10-14]
LEVEL = 4 -> HEMT2 Model, Maquarie University
LEVEL = 5 -> Curtis-Ettenburg GaAs Model

Level 1 is derived from the GaAs FET model of Statz and is the same as in Berkeley SPICE 3. It is the default model level selected if no level=# model parameter is detected. It is modeled as an intrinsic FET with ohmic resistances in series with the drain and source. The DC characteristics are defined by the parameters VTO, B, and BETA, which determine the variation of drain current with gate voltage, ALPHA, which determines saturation voltage, and LAMBDA, which determines the output conductance. Two ohmic resistances, RD and RS, are included. Charge storage is modeled by total gate charge as a function of gate-drain and gate-source voltages and is defined by the parameters CGS, CGD, and PB.

Statz MESFET Model Parameters

Name	Parameter	Units	Default	Example	Area
VTO	pinch-off voltage	V	-2.0	-2.0	
BETA	transconductance parameter	A/V^2	1e-4	1e-3	*
B	doping tail extending parameter	1/V	0.3	0.3	*
ALPHA	saturation voltage parameter	1/V	2	2	*
LAMBDA	channel length modulation parameter	1/V	0	1e-4	
RD	drain ohmic resistance	Ω	0	100	/
RS	source ohmic resistance	Ω	0	100	/
CGS	zero-bias G-S junction capacitance	F	0	.1pF	*
CGD	zero-bias G-D junction capacitance	F	0	.05pF	*
PB	gate junction potential	V	1	0.6	
IS	gate junction saturation current	A	1e-14	1e-14	*
KF	flicker noise coefficient	-	0		
AF	flicker noise exponent	-	1		
FC	coefficient for forward-bias depletion capacitance formula	-	0.5		

Statz Model Examples

```
.MODEL NE760 NMF (VTO=-1 BETA=.1275 B=.3 ALPHA=2
+ LAMBDA=15.5M RD=5.45 RS=4.88 IS=19.8P PB=1 FC=.2
+ CGS=.34P CGD=.03P)

.MODEL NE710 NMF (VTO=-2 BETA=.047 B=.3 ALPHA=2
+ LAMBDA=15.5M RD=1.13 RS=1.94 IS=7.31P PB=1 FC=.2
+ CGS=.45P CGD=.1P)
```

See references in Volume 2, at the end of Chapter 10 for more information.

HEMT Model Parameters

Name	Parameter
a	1st electron density parameter 2DEG
b	MESFET Doping tail or 2nd electron density parameter 2DEG
c	3rd electron density parameter 2DEG
level	Order of ns polynomial 2DEG
ma	1st electron density parameter Parasitic MESFET
mb	2nd electron density parameter Parasitic MESFET
length	Gate length
alpha	Saturation voltage parameter or Vdss adjustment factor
malpha	mVdss adjustment factor
vpoly	Order of Vdss polynomial 2DEG
vgg	Root of Vdss polynomial 2DEG
vpoly	Vdss polynomial adjustment factor 2DEG
ec	Critical electric field for velocity saturation 2DEG
vsat	Saturated electron velocity 2DEG
mvpoly	Order of mVdss polynomial Parasitic MESFET
mvgg	Root of mVdss polynomial Parasitic MESFET
mvpoly	mVdss polynomial adjustment factor Parasitic MESFET
mec	Critical electric field for velocity saturation Parasitic MESFET
mvsat	Saturated electron velocity Parasitic MESFET
n	Emission coefficient
gamma	Vds-saturation smoothing parameter for capacitance 2DEG
mgamma	Vds-saturation smoothing parameter for capacitance Parasitic MESFET
eta	Second gate effect parameter 2DEG
meta	Second gate effect parameter Parasitic MESFET
mlambda	Par. MESFET channel length modulation parm.
mvto	Pinch-off voltage Parasitic MESFET
mlinpow	Power for linear region approximation Parasitic MESFET
linpow	Power for linear region approximation
cgsp	G-S Peripheral capacitance
cgdp	G-D Peripheral capacitance

Curtis-Ettenburg Model Parameters	
Name	**Parameter**
lg	gate inductance
ld	drain inductance
ls	source inductance
is	Junction Saturation Current
vbi	Effective Builtin Potential
tau	Internal Delay for Vin
cds	Capacitance of D-S at zero bias
cgso	Capacitance of G-S at zero bias
cgdo	Capacitance of G-D at zero bias
a0	Coefficient Zero
a1	Coefficient One
a2	Coefficient Two
a3	Coefficient Three
beta	Transconductance parameter
gamma	Saturation Voltage Parameter
rdso	Ids Channel-Length Modulation resistance parameter
vdsdc	Ids Channel-Length Modulation voltage parameter
vdso	Output Voltage where As are Evaluated
vds0	Output Voltage where As are Evaluated
vbr	Break down voltage from D-G
rg	Gate Ohmic Resistance
rd	Drain ohmic resistance
rs	Source ohmic resistance
fc	Junction Capacitance breakpoint for 2 models
crf	AC Correction Factor 1
rc	AC Correction Factor 2
vt0	Pinch-off voltage
vto	Pinch-off voltage
n	factor of diode model

```
.MODEL NMES PMF (level=5 RD=2.6 RG=4.0 RS=2.6
+ A0=.1 A1=.0492 vbi=.8 A2=-.0025 A3=-.001667 RDSO=300
+ VDSO=3.0 GAMMA=3.0 VBR=20 vto=-3 beta=0 vdsdc=0
+ n=1 is=1e-14 cgso=.3p cgdo=30f cds=.3p fc=.5 tau=5p)
```

Metal Oxide Field Effect Transistors - MOSFETs

Format: M*name ND NG NS NB modname*
+ [L=*lenval*] [W=*wval*] [AD=*adval*] [AS=*asval*]
+ [PD=*pdval*] [PS=*psval*] [NRD=*nrdval*]
+ [NRS=*nrsval*] [OFF] [IC=*vds,vgs,vbs*] [TEMP=*t*]
+ [M=value]

Examples: M1 24 2 0 20 TYPE1
M31 2 17 6 10 MODM L=5U W=2U
M1 2 9 3 0 MOD1 L=10U W=5U AD=100P
+AS=100P PD=40U PS=40U

Mosfet calls begin with the letter M. *ND*, *NG*, *NS*, and *NB* are the drain, gate, source, and bulk (substrate) nodes, respectively. *Modname* is the model name. L and W are the channel length and width, in meters. AD and AS are the areas of the drain and source diffusions, in meters^2. Note that the suffix 'U' specifies microns (1E-6 m) and 'P' sq-microns (1E-12 m^2). If any of L, W, AD, or AS values are not specified, then the default values are used. The use of defaults simplifies input file preparation, as well as the editing required if the device geometries are to be changed. The .OPTIONS parameters DEFL, DEFW, DEFAD, and DEFAS can be used to set the default values for the L, W, AD, and AS parameters, respectively. PD and PS are the perimeters of the drain and source junctions, in meters. NRD and NRS designate the equivalent number of squares of the drain and source diffusions; these values multiply the sheet resistance RSH specified on the .MODEL statement giving the parasitic series drain and source resistance values. PD and PS default to zero, while NRD and NRS default to 1. OFF indicates an initial condition for DC analysis. The initial condition specification, using IC=*vds,vgs,vbs,* is intended for use with the UIC option on the .TRAN line. It should be used when you desire a specific initial condition, other than the operating point value, at the beginning of the transient analysis. The (optional) TEMP value is the temperature at which this device is to operate and overrides the temperature specification in the .OPTIONS statement.M is the multiplicity factor that simulates parallel devices. The temperature specification is only valid for model levels 1, 2, 3, and 6. It is not valid for the BSIM models.

The MOSFET Models

IsSpice4 provides a variety of MOS models, which differ widely in behavior. The level parameter specifies the model to be used, except in the case of the C Code model, which uses an alternate model type and keyletter:

LEVEL = 1 -> Shichman-Hodges
LEVEL = 2 -> MOS2 (as described in reference [10-4])
LEVEL = 3 -> MOS3, a semi-empirical model (see reference [10-4])
LEVEL = 4 -> BSIM 1 (as described in reference [10-5])
LEVEL = 5 -> BSIM 2 (as described in reference [10-6])
LEVEL = 6 -> MOS6 (as described in reference [10-7])
LEVEL = 7&8 -> BSIM3v3.2.4 (as described in reference [10-12])
LEVEL = 9 -> EPLF-EKV V 2.6
LEVEL =10 -> BSIMSOIv3.2 (Silicon-On-Insulator)
LEVEL =14&15-> BSIM4V4.6.1
AHDL Model -> Fully Depleted SOI MOSFET C Code Model [9-1. 9-2. 9-3]

Berkeley SPICE Level 1, 2, and 3

The DC characteristics of the level 1 through level 3 MOSFETs are defined by the device parameters VTO, KP, LAMBDA, PHI and GAMMA. These parameters are computed by IsSpice4 if the process parameters (NSUB, TOX,..., etc.) are given, but user-specified values always override the computed values. VTO is positive for enhancement mode and negative for depletion mode N-channel devices. VTO is negative for enhancement mode and positive for depletion mode P-channel devices. Charge storage is modeled by:

- Three constant capacitors, CGSO, CGDO, and CGBO, which represent overlap capacitances,
- The nonlinear thin-oxide capacitance, which is distributed among the gate, source, drain, and bulk regions, and
- The nonlinear depletion-layer capacitances for both substrate junctions, divided into bottom and periphery capacitances. These capacitors vary as the MJ and MJSW power of the junction voltage, respectively, and are determined by the parameters CBD, CBS, CJ, CJSW, MJ, MJSW and PB.

Charge storage effects are modeled by the piecewise linear voltage-dependent capacitance model by Meyer (see references [6-1, 6-11] in Working with Model Libraries). The thin-oxide charge storage effects are treated differently for the level 1 model. These voltage-dependent capacitances are included only if TOX is specified and they are represented using Meyer's formulation.

The Meyer model used in other versions of SPICE 2 is not the original Meyer model proposed for SPICE 2, but a variation (see reference [6-8] in Working with Model Libraries). Unfortunately, the modifications, which were intended to include bulk voltage effects, cause the gate-drain and gate-source capacitances to be discontinuous when Vds crosses zero, thus causing a number of convergence problems. Additionally, due to the fact that the Meyer model did not conserve charge, the Ward Dutton charge conserving model (see reference[6-4] of the Working with Model Libraries book) was added as an option.

In IsSpice4, the MOSFET capacitance model has been replaced with the original Meyer model. This should solve many of the "Timestep too small" problems encountered in SPICE 2. At this time, there is no charge conserving model in IsSpice4. Therefore, the XQC parameter, which triggered use of the Ward Dutton model, is not valid.

There is some overlap among the parameters describing the junctions, e.g. the reverse current can be input either as IS (in A) or as JS (in A/m^2). Whereas the first is an absolute value, the second is multiplied by AD and AS to give the reverse current of the drain and source junctions, respectively. This methodology has been chosen since there is no sense in always relating junction characteristics with AD and AS entered on the device call line; the areas can be defaulted using the .OPTIONS statement. The same idea also applies to the zero-bias junction capacitances, CBD and CBS (in F), on one hand, and CJ (in F/m^2) on the other. The parasitic drain and source series resistances can be expressed as either RD and RS (in ohms), or RSH (in ohms/sq.), with the latter multiplied by the number of squares, NRD and NRS, entered on the device call line.

A discontinuity in the MOS level 3 model with respect to the KAPPA parameter has been corrected. Since this fix may affect parameter fitting, the .OPTIONS parameter "BADMOS3" can be set to use the old MOS level 3 model.

MOSFET Level 1, 2, & 3 Model Parameters

Name	Parameter	Units	Default	Example
LEVEL	model index	-	1	
VTO	zero-bias threshold voltage	V	0.0	1.0
KP	transconductance parameter	A/V^2	2e-5	3.1e-5
GAMMA	bulk threshold parameter	$V^{.5}$	0.0	0.37
PHI	surface potential	V	0.6	0.65
LAMBDA	channel-length modulation (MOS1 and MOS2 only)	V^{-1}	0.0	0.02
RD 1.0	drain ohmic resistance	Ω		0.0
RS 1.0	source ohmic resistance	Ω		0.0
CBD	zero-bias B-D junction capacitance	F	0.0	20fF
CBS	zero-bias B-S junction capacitance	F	0.0	20fF
IS	bulk junction saturation current	A	1e-14	1e-15
PB	bulk junction potential	V	0.8	0.87
CGSO	gate-source overlap capacitance per meter channel width	F/m	0.0	4e-11
CGDO	gate-drain overlap capacitance per meter channel width	F/m	0.0	4e-11
CGBO	gate-bulk overlap capacitance per meter channel length	F/m	0.0	2e-10
RSH	drain and source diffusion sheet resistance	Ω/sq.	0.0	10.0
CJ	zero-bias bulk junction bottom cap. per sq-meter of junction area	F/m^2	0.0	2e-4
MJ	bulk junction bottom grading coefficient	-	0.5	0.5
CJSW	zero-bias bulk junction sidewall cap. per meter of junction perimeter	F/m	0.0	1e-9
MJSW	bulk junction sidewall grading coefficient	-	0.50(level 1) 0.33(level 2, 3)	

MOSFET Level 1, 2, & 3 Model Parameters, *continued*

Name	Parameter	Units	Default	Example
JS	bulk junction saturation current per sq-meter of junction area	A/m^2	0	1e-8
TOX	oxide thickness	meter	1e-7	1e-7
NSUB	substrate doping	cm^{-3}	0.0	4e15
NSS	surface state density	cm^{-2}	0.0	1e10
NFS	fast surface state density	cm^{-2}	0.0	1e10
TPG	type of gate material: +1 opposite to substrate -1 same as substrate 0 Al gate	-	1.0	
XJ	metallurgical junction depth	meter	0.0	1u
LD	lateral diffusion	meter	0.0	0.8u
UO	surface mobility	$cm^2/V\text{-}s$	600	700
UCRIT	critical field for mobility degradation (MOS2 only)	V/cm	1e4	1e4
UEXP	critical field exponent in mobility degradation (MOS2 only)	-	0.0	0.1
UTRA	transverse field coefficient (mobility) (deleted for MOS2)	-	0.0	0.3
VMAX	maximum drift velocity of carriers	m/s	0.0	5e4
NEFF	total channel charge (fixed and mobile) coefficient (MOS2 only)	-	1.0	5.0
KF	flicker noise coefficient	-	0.0	1e-26
AF	flicker noise exponent	-	1.0	1.2
FC	coefficient for forward-bias depletion capacitance formula	-	0.5	
DELTA	width effect on threshold voltage (MOS2 and MOS3)	-	0.0	1.0
THETA	mobility modulation (MOS3 only)	V^{-1}	0.0	0.1
ETA	static feedback (MOS3 only)	-	0.0	1.0
KAPPA	saturation field factor (MOS3 only)	-	0.2	0.5
ALPHA	alpha (MOS3 only)	-	0.0	-
XD	depletion layer width (MOS3 only)	-	0.0	-
TNOM	parameter measurement temp.	°C	27	50

```
.MODEL SST211 NMOS (LEVEL=1 VTO=0.8 KP=1E-02
+ GAMMA=5.E-06 PHI=0.75 LAMBDA=1.40E-02 RD=3.00E+01
+ RS=3.60E+01 IS=3.25E-14 CBD=5.13E-12 CBS=6.16E-12 PB=0.80
+ MJ=.46 TOX=3.00E-07 CGSO=3.60E-09 CGDO=3.00E-09
+ CGBO=2.34E-08)
```

Sample Models 2 µm CMOS Level 2 Models supplied by MOSIS® :

```
.MODEL NMOSIS NMOS LEVEL=2 LD=0.25U TOX=429E-10
+ NSUB=5.3087E+15 VTO=0.796 KP=4.991E-5 GAMMA=0.5215
+ PHI=0.6 UO=620.030 UEXP=0.1695 UCRIT=76799.6
+ DELTA=4.4485 VMAX=1E+5 XJ=0.25U LAMBDA=1.6208E-2
+ NFS=2.06E+11 NEFF=1 NSS=1E+10 TPG=1 RSH=30.94
+ CGDO=3.0185E-10 CGSO=3.0185E-10 CGBO=3.8275E-10
+ CJ=1.0159E-4 MJ=0.6306 CJSW=4.744E-10 MJSW=.315 PB=0.8

.MODEL PMOSIS PMOS LEVEL=2 LD=0.25U TOX=429E-10
+ NSUB=5.3093E+15 VTO=-0.8078 KP=2.157E-5 GAMMA=.5216
+ PHI=0.6 UO=267.981 UEXP=0.1297 UCRIT=5000
+ DELTA=1.3792 VMAX=1E+5 XJ=0.25U LAMBDA=2.724E-2
+ NFS=2.77E+11 NEFF=1.001 NSS=1E+10 TPG=-1 RSH=89.08
+ CGDO=3.0185E-10 CGSO=3.0185E-10 CGBO=4.054E-10
+ CJ=2.3837E-04 MJ=0.5353 CJSW=2.76E-10 MJSW=0.253 PB=0.8

.MODEL VN0603L NMOS (LEVEL=3 VTO=2.5 KP=.23
+ GAMMA=1.93U THETA=.24 PHI=.75 LAMBDA=1.25M RD=.49
+ RS=.49 IS=62.5F PB=.8 MJ=.46 CBD=544.4P CBS=753P
+ CGSO=4.5U CGDO=320N CGBO=760N)
```

Berkeley Short-Channel IGFET Model (BSIM1, 2, and 3)

The BSIM (level 4, 5, and 7/8) parameter values are obtained from process characterization, and can be generated automatically. For BSIM1/2 Ref. [10-5] in Working with Model Libraries describes a means of generating a 'process' file that can be converted into a sequence of .MODEL lines for inclusion in an IsSpice4 circuit file. Parameters marked in the table with an * in the l/w column also have corresponding parameters with a length and width dependency. For example, VFB (flat-band voltage), with units of Volts, has 2 related parameters, LVFB and WVFB, which have units of Volt-µmeter The formula:

$$P = P_o + \frac{P_L}{L_{effective}} + \frac{P_w}{W_{effective}}$$

is used to evaluate the parameter value for the actual device specified with:

$$L_{effective} = L_{input} - DL$$

and

$$W_{effective} = W_{input} - DW$$

Note that unlike the other models in IsSpice4, the BSIM models are designed for use with a process characterization system that provides all the parameters. Therefore, there are no defaults for the parameters and leaving one parameter out is considered an error. See ref. [10-5] for more information.

MOSFET BSIM 1 (Level 4) Model Parameters

Name	Parameter	Units	I/w
VFB	flat-band voltage	V	*
PHI	strong inversion surface potential	V	*
K1	body effect coefficient	$V^{.5}$	*
K2	drain/source depletion charge sharing coefficient	-	*
ETA	zero-bias drain-induced barrier lowering coefficient	-	*
MUZ	zero-bias mobility (at Vds=0 Vgs=Vth)	$cm^2/V\text{-}s$	
DL	channel length reduction	µm	
DW	channel width reduction	µm	
U0	zero-bias transverse-field mobility degradation coefficient	V^{-1}	*
U1	zero-bias velocity saturation coefficient	µm/V	*
X2MZ	sens. of mobility to substrate bias at vds=0	$cm^2/V^2\text{-}s$	*
X2E	sens. of drain induced barrier lowering effect to substrate bias	V^{-1}	*
X3E	sens. of drain induced barrier lowering effect to drain bias at Vds=Vdd	V^{-1}	*
X2U0	sens. of transverse field mobility degradation effect to substrate bias	V^{-2}	*
X2U1	sens. of velocity saturation effect to substrate bias	$µm/V^2$	*
X3U1	sens. of velocity saturation effect on drain bias at Vds=Vdd	$µm/V^2$	*
MUS	mobility at zero substrate bias and Vds=Vdd	$cm^2/V^2\text{-}s$	
X2MS	sens. of mobility to substrate bias at Vds=Vdd	$cm^2/V^2\text{-}s$	*
X3MS	sens. of mobility to drain bias at Vds=Vdd	$cm^2/V^2\text{-}s$	*
TOX	gate oxide thickness	µm	
TEMP	temperature at which parameters were measured	°C	
VDD	measurement bias range (for MUS)	V	
CGDO	gate-drain overlap cap. per meter channel width	F/m	
CGSO	gate-source overlap cap. per meter channel width	F/m	
CGBO	gate-bulk overlap cap. per meter channel length	F/m	
XPART	gate-oxide capacitance charge model flag	-	
N0	zero-bias subthreshold slope coefficient	-	*

MOSFET BSIM 1 (Level 4) Model Parameters			
Name	**Parameter**	**Units**	**l/w**
NB	sens. of subthreshold slope to substrate bias	-	*
ND	sens. of subthreshold slope to drain bias	-	*
RSH	drain and source diffusion sheet resistance	Ω/sq.	
JS	source-drain junction current density	A/m^2	
PB	built-in potential of source-drain junction	V	
MJ	grading coefficient of source-drain junction bottom	-	
PBSW	built in potential of source-drain junction sidewall	V	
MJSW	grading coefficient of source-drain junction sidewall	-	
CJ	source-drain junction capacitance per unit area	F/m^2	
CJSW	source-drain junction sidewall cap. per unit length	F/m	
WDF	source-drain junction default width	m	
DELL	source-drain junction length reduction	m	

XPART:XPART+0selects a 40/60 drain/source charge partition in saturation, while
XPART=1 selects a 0/100 drain/source charge partition

BSIM3 is a physical model and is based on a coherent quasi two-dimensional analysis of the MOSFET device structure, taking into account the effects of device geometry and process parameters. In other words, dependencies of important geometry and process parameters such as channel length, channel width, gate oxide thickness, junction depth, substrate doping concentration, etc. are built into the model. BSIM3 allows users to accurately model MOSFET behavior over a wide range of existing technologies and predict the behavior for future technologies. See http://www-device.eecs.berkeley.edu/intro.html for more information on BSIM3.

The BSIM3v3 (version 3.2) model has been extensively modified from previous releases and is the recommended version. Some of the modifications that are not found in version 2 are:

- A single I-V expression is used to model current and output conductance characteristics for subthreshold, strong inversion, linear, and saturation regions. This formulation guarantees continuity for **Ids**, **Gds**, **Gm** and their derivatives for all **Vgs** and **Vds** bias conditions.

- There are new width dependencies for bulk charge and source/ drain resistance, **Rds**. This greatly enhances the accuracy of the model for narrow width devices.

- **dw** and **dl** dependencies are available for different Wdrawn and Ldrawn devices. This improves the model's ability to fit a variety of **W/L** ratios with a single set of parameters.

- New capacitance equations improve the modeling of short and narrow geometry devices.

- New relaxation time model for characterizing the non-quasi-static effect of MOS circuits for improved transient behavior.

MOSFET BSIM 2 (Level 5) Model Parameters

Name	Parameter	I/w
VFB	flat-band voltage	*
PHI	strong inversion surface potential	*
K1	body effect coefficient	*
K2	drain/source depletion charge sharing coefficient	*
ETA0	zero-bias drain-induced barrier lowering coefficient	*
ETAB	sens. of drain induced barrier lowering effect to substrate bias	*
DL	channel length reduction	
DW	channel width reduction	
MU0	low-field mobility (at Vds=0 Vgs=Vth)	
MU0B	sens. of mobility to substrate bias at vds=0	*
MUS0	mobility at zero substrate bias and Vds=Vdd	*
MUSB	sens. of mobility to substrate bias at Vds=Vdd	*
MU20	Vds dependence of MU in tanh term	*
MU2B	sens. of mobility to substrate bias at Vds=vdd	*
MU2G	sens. of mobility to gate bias	*
MU30	Vds dependence of MU in linear term	*
MU3B	sens. of mobility to substrate bias at Vds=vdd	*
MU3G	sens. of mobility to gate bias	*
MU40	Vds dependence of MU in linear term	*
MU4B	sens. of mobility to substrate bias at Vds=vdd	*
MU4G	sens. of mobility to gate bias	*

MOSFET BSIM 2 (Level 5) Model Parameters, *continued*

Name	Parameter	I/w
UA0	zero-bias transverse-field linear mobility degradation coefficient	*
UAB	sens. of transverse field mobility degradation effect to substrate bias	*
UB0	zero-bias transverse-field quadratic mobility degradation coefficient	*
UBB	sens. of transverse field mobility degradation effect to substrate bias	*
U10	zero-bias velocity saturation coefficient	*
U1B	sens. of velocity saturation effect to substrate bias	*
U1D	sens. of velocity saturation effect to drain bias	*
N0	zero-bias subthreshold slope coefficient	*
ND	sens. of subthreshold slope to drain bias	*
VOF0	Threshold voltage offset at Vds, Vbs=0	*
VOFB	sens. of voltage offset to substrate bias	*
VOFD	sens. of voltage offset to drain bias	*
AI0	pre-factor of hot-electron effect	*
AIB	sens. of pre-factor effect to substrate bias	*
BI0	exponential factor of hot-electron effect	*
BIB	sens. of exponential factor to substrate bias	*
VGHIGH	upper bound of the cubic spline function	*
VGLOW	lower bound of the cubic spline function	*
TOX	gate oxide thickness	
TEMP	temperature at which parameters were measured	
VDD	measurement bias range	
VGG	measurement bias range	
VBB	measurement bias range	
CGDO	gate-drain overlap cap. per meter channel width	
CGSO	gate-source overlap cap. per meter channel width	
CGBO	gate-bulk overlap cap. per meter channel length	
XPART	gate-oxide capacitance charge model flag	
RSH	drain and source diffusion sheet resistance	
JS	source-drain junction current density	
PB	built-in potential of source-drain junction	
MJ	grading coefficient of source-drain junction	
PBSW	built-in potential of source-drain junction sidewall	
MJSW	grading coefficient of source-drain junction sidewall	
CJ	source-drain junction capacitance per unit area	

MOSFET BSIM 2 (Level 5) Model Parameters, *continued*		
Name	**Parameter**	**I/w**
CJSW	source-drain junction sidewall cap. per unit length	
WDF	source-drain junction default width	
DELL	source-drain junction length reduction	

XPART If XPART= 0 selects a 40/60 drain/source charge partition in saturation, while XPART = 1 selects a 0/100 drain/source charge partition.

MOSFET Level 6 Model Parameters

Name	Parameter	Units	Default	Example
VTO	zero-bias threshold voltage	V	0.0	0.6
KV	saturation voltage factor	-	2.0	0.9
NV	saturation voltage coefficient	-	0.5	0.87
KC	saturation current factor	-	5e-5	3.8e-5
NC	saturation current coefficient	-	1	1.2
NVTH	threshold voltage coefficient	V	0.5	0.6
PS	saturation current modification parameter	V	0.0	0.0
GAMMA	bulk threshold parameter	$V^{.5}$	0.0	0.6
GAMMA1	bulk threshold parameter1	$V^{.5}$	0.0	0.37
SIGMA	static feedback effect parameter	$V^{.5}$	0.0	0.37
PHI	surface potential	V	0.6	1.0
LAMBDA	channel-length modulation	V^{-1}	0.0	0.02
LAMBDA0	channel-length modulation 0	V^{-1}	0.0	0.06
LAMBDA1	channel-length modulation 1	V^{-1}	0.0	0.003
RD	drain ohmic resistance	Ω	0.0	1.0
RS	source ohmic resistance	Ω	0.0	1.0
CBD	zero-bias B-D junction cap.	F	0.0	20fF
CBS	zero-bias B-S junction cap.	F	0.0	20fF
IS	bulk junction saturation current	A	1e-14	1e-15
PB	bulk junction potential	V	0.8	0.87
CGSO	gate-source overlap capacitance per meter channel width	F/m	0.0	4e-10
CGDO	gate-drain overlap capacitance per meter channel width	F/m	0.0	4e-10
CGBO	gate-bulk overlap capacitance per meter channel length	F/m	0.0	2e-10
RSH	drain and source diffusion sheet resistance	Ω/sq.	0.0	10.0
CJ	zero-bias bulk junction bottom cap. per sq-meter of junction area	F/m^2	0.0	2e-4
MJ	bulk junction bottom grading coefficient	-	0.5	0.429

MOSFET Level 6 Model Parameters, *continued*				
CJSW	zero-bias bulk junction sidewall cap. per meter of junction perimeter	F/m	0.0	1e-10
MJSW	bulk junction sidewall grading coefficient	-	0.5	0.35
JS	bulk junction saturation current per sq-meter of junction area	A/m^2	1e-8	
LD	lateral diffusion	meter	0.0	0.28u
TOX	oxide thickness	meter	1e-7	1.9e-8
UO	surface mobility	$cm^2/V\text{-}s$	600	700
FC	coefficient for forward-bias depletion capacitance formula	-	0.5	
TPG	type of gate material: +1 opp. to substrate -1 same as substrate 0 Al gate	-	1.0	
NSUB	substrate doping	cm^{-3}	0.0	4e15
NSS	surface state density	cm^{-2}	0.0	1e10
TNOM	parameter measurement temp.	°C	27	50

The level 6 model describes a simple, general purpose model. that is valid for short channel Mosfets with channel lengths down to ≈.25µm, GaAs FETs, and resistance inserted Mosfets. The model is superior in speed to the level 3 model, running about 3 times faster. For more information, see reference [6-7] of the Working with Model Libraries book.

Sample Models
Level 6 Models:

```
.MODEL N10L5 NMOS (LEVEL=6 TPG=1 KC=3.8921e-05
+ NC=1.1739 KV=0.91602 NV=0.87225
+ LAMBDA0=0.013333 LAMBDA1=0.0046901 VT0=0.69486
+ GAMMA=0.60309 PHI=1 TOX=1.98E-08
+ LD=0.1U NSUB=4.99E+16 NSS=0 CJ=4.091E-4
+ MJ=0.307 PB=1.0 CJSW=3.078E-10 MJSW=1.0E-2
+ CGSO=3.93E-10 CGDO=3.93E-10
```

BSIM3 Note: *BSIM3 version 2 model parameters are not listed in the manual. Only the lastest BSIM3 (version 3.2.4) parameters are listed here.*

In addition to the instance parameters listed on page 206, the following additional instance parameters may be used for BSIM3 models.

Name	Parameter
NQSMOD	Non-quasi-static model selector

BSIM3 Version 3.2 Level 8, *continued*

MOSFET, BSIM3 Version 3.2 Level 8 Model Parameters

Parameter	Description	Default	Unit
Used in IsSpice4			
Model Control Parameters			
level	BSIM3v3 model selector	8	none
mobmod	Mobility model selector	1	none
capmod	Flag for the short channel capacitance model	2	none
nqsmod	Flag for the NQS model	0	none
noimod	Noise model selector	1	none
	For noimode=1 Spice2 fliker noise model+ Spice2 thermal noise model		
	For noimode=2 BSIM3 fliker noise model+ BSIM3 thermal noise model		
	For noimode=3 BSIM3 fliker noise model+ Spice2 thermal noise model		
	For noimode=4 Spice2 fliker noise model+ BSIM3 thermal noise model		
Nqsmod	Non-quasi-static model selector		
paramchk	Parameter Warning Checking	off	
version	BSIM3 version number	3.1	
DC Parameters			
vth0	Threshold voltage @Vbs=0 for large L.	0.7 for NMOS	V
	Typically Vth0 > 0 for NMOSFET and Vth0 < 0 for PMOSFET	-0.7 for PMOS	V
k1	First-order body effect coefficient	0	$V^{1/2}$
k2	Second-order body effect coefficient	0	none
k3	Narrow width coefficient	80	none
k3b	Body effect coefficient of K3	0	1/V
w0	Narrow width parameter	2.5E-6	m
nlx	Lateral non-uniform doping coefficient	1.74E-7	m
vbm	Maximum applied body bias in Vth calculation	-3	V
dvt0	First coeff. of short channel effect on Vth	2.2	none
dvt1	Second coeff. of short channel effect on Vth	0.53	none
dvt2	Body-bias coeff. of short channel effect on Vth	-0.032	1/V
dvt0w	First coefficient of narrow width effect on Vth at small L	0	none
dvt1w	Second coefficient of narrow width effect on Vth at small L	5.3E6	1/m
dvt2w	Body-bias coefficient of narrow width effect on Vth at small L	-0.032	1/V
u0	Mobility at Temp=Tnom NMOSFET	0.067	m^2/Vs
	Mobility at Temp=Tnom PMOSFET	0.025	m^2/Vs
ua	First-order mobility degradation coefficient	2.25E-9	m/V
ub	Second-order mobility degradation coefficient	5.87E-19	$(m/V)^2$
uc	Body-effect of mobility degradation coefficient		

BSIM3 Version 3.2 Level 8, *continued*

Parameter	Description	Default	Unit
	Mobmod=1,2:	-4.65E-11	m/V^2
	Mobmod=3:	-0.0465	m/V^2
vsat	Saturation velocity at Temp=Tnom	8.0E4	m/sec
a0	Bulk charge effect coefficient for channel length	1	none
ags	Gate bias coefficient of Abulk	0	1/V
b0	Bulk charge effect coefficient for channel width	0	m
b1	Bulk charge effect width offset	0	m
keta	Body-bias coefficient of the bulk charge effect	-0.047	1/V
a1	First non-saturation factor	0	1/V
a2	Second non-saturation factor	1	none
rdsw	Parasitic resistance per unit width	0	Ω - μm^{Wr}
prwb	Body effect coefficient of Rdsw	0	$V^{-1/2}$
prwg	Gate bias effect coefficient of Rdsw	0	1/V
wr	Width offset from Weff for Rds calculation	1	none
wint	Width offset fitting param from I-V w/o bias	0	m
lint	Length offset fitting param from I-V w/o bias	0	m
dwg	Coefficient of Weff's gate dependence	0	m/V
dwb	Coefficient of Weff's substrate body bias dependence	0	$m/V^{1/2}$
voff	Offset voltage in the subthreshold region at large W and L	-0.08	V
nfactor	Subthreshold swing factor	1	none
eta0	DIBL coefficient in the subthreshold region	0.08	none
etab	Body-bias coeff for the subthreshold DIBL effect	-0.07	1/V
dsub	DIBL coeff exponent in subthreshold region	0.56 (drout)	none
cit	Interface trap capacitance	0	F/m^2
cdsc	Drain/source to channel coupling capacitance	2.4E-4	F/m^2
cdscb	Body-bias sensitivity of Cdsc	0	F/Vm^2
cdscd	Drain-bias sensitivity of Cdsc	0	F/Vm^2
pclm	Channel length modulation parameter	1.3	none
pdiblc1	First output resistance DIBL effect correction parameter	0.39	none
pdiblc2	Second output resistance DIBL effect correction parameter	0.0086	none
pdiblcb	Body effect coefficient of DIBL correction parameters	0	1/V
drout	L dependence coefficient of the DIBL correction parameter in Rout	0.56	none
pscbe1	First substrate current body-effect parameter	4.24E8	V/m
pscbe2	Second substrate current body-effect parameter	1.0E-5	m/V
pvag	Gate dependence of early voltage	0	none
delta	Effective Vds parameter	0.01	V

BSIM3 Version 3.2 Level 8, *continued*

Parameter	Description	Default	Unit
ngate	Poly gate doping concentration	0	cm^{-3}
alpha0	First parameter of impact ionization current	0	m/V
beta0	Second parameter of impact ionization current	30	V
rsh	Source-drain sheet resistance	0	Ω/square
jssw	Sidewall saturation current density	0	A/m
js	Source-drain junction saturation current	1.0E-4	A/m^2
AC and Capacitance Parameters			
xpart	Charge partitioning rate flag	0	none
cgs0	Non LDD region source-gate overlap capacitance per channel length	(calculated)	F/m
cgd0	Non LDD region drain-gate overlap capacitance per channel length	(calculated)	F/m
cgb0	Gate bulk overlap capacitance per unit channel length	2 * Dwe * Cox	F/m
cj	Source and drain bottom junction	5.0E-4	F/m^2
mj	Bottom junction capacitance grating coefficient	0.5	
mjsw	Source/Drain side junction capacitance grading coefficient	0.33	none
cjsw	Source/Drain side junction capacitance	5.0E-10	F/m^2
cjswg	Source/drain gate side wall junction cap.	5E-10 (Cjsw)	
mjswg	Source/drain gate side wall junction grading coefficient	0.33 (Mjsw)	none
pbsw	Source/Drain side junction built-in potential	1	V
pb	Bottom junction built-in potential	1	V
pbswg	Source/drain gate side wall junction built-in potential	1.0 (Pbsw)	V
cgsl	Light doped source-gate region overlap cap.	0	F/m
cgdl	Light doped drain-gate region overlap cap.	0	F/m
ckappa	Coefficient for lightly doped region overlap fringing field capacitance	0.6	F/m
cf	Fringing field capacitance	7.3E-11 (calculated)	F/m
clc	Constant term for the short channel mode	0.1E-6	m
cle	Exponential term for the short channel mode	0.6	none
dlc	Length offset fitting parameter from C-V	0 (lint)	m
dwc	Width offset fitting parameter from C-V	0 (wint)	m
vfb	Flat-band voltage parameter (for capmod=0)	-1	V
NQS Model Parameters			
elm	Elmore constant of the channel	5	none

BSIM3 Version 3.2 Level 8, *continued*

Parameter	Description	Default	Unit
W and L Parameters			
wl	Coefficient of length dependence for width offset	0	m^{Wln}
wln	Power of length dependence of width offset	1	none
ww	Coefficient of width dependence for width offset	0	m^{Wwn}
wwn	Power of width dependence of width offset	1	none
wwL	Coefficient of length and width cross term for width offset	0	$m^{Wwn+Wln}$
ll	Coefficient of length dependence for length offset	0	m^{Lln}
lln	Power of length dependence for length offset	1	none
lw	Coefficient of width dependence for length offset	0	m^{Lwn}
lwn	Power of width dependence for length offset	1	none
lwL	Coefficient of length and width cross term for length offset	0	$m^{Lwn+Lln}$
ub1	Temperature coefficient for Ub	-7.61E-18	$(m/V)^2$
uc1	Temperature coefficient for Uc		
	Mobmod=1,2:	-5.6E-11	m/V^2
	Mobmod=3:	-0.056	m/V^2
at	Temperature coefficient for saturation velocity	3.3E4	m/sec
Temperature Effect Parameters			
tnom	Temperature at which parameters are extracted	27^oC	
ute	Mobility temperature exponent	-1.5	none
kt1	Temperature coefficient for threshold voltage	-0.11	V
kt1L	Channel length sensitivity of the temperature coefficient for threshold voltage	0	V∗m
kt2	Body-bias coefficient of the Vth temperature effect	0.022	none
ua1	Temperature coefficient for Ua	4.31E-9	m/V
ub1	Temperature coefficient for Ub	-7.61E-18	$(m/V)^2$
uc1	Temperature coefficient for Uc		
	Mobmod=1,2:	-5.6E-11	m/V^2
	Mobmod=3:	-0.056	m/V^2
at	Temperature coefficient for saturation velocity	3.3E4	m/sec
prt	Temperature coefficient for Rdsw	0	Ω– µm
nj	Emission coefficient of junction	1	none
xti	Junction current temperature exponent coefficient	3.0	none

BSIM3 Version 3.2 Level 8, *continued*

Parameter	Description	Default	Unit
Noise Model Parameters			
Noia	Noise parameter A	NMOS 1.0E20 PMOS 9.9E18	none
Noib	Noise parameter B	NMOS 5.0E4 PMOS 2.4E3	none
Noic	Noise parameter C	NMOS -1.4E-12 PMOS -1.4E-12	none
em	Saturated field	4.1E7	V/m
af	Flicker frequency exponent for noimod=1	1	none
ef	Flicker frequency exponent for noimod=2	1	none
kf	Flicker noise parameter for noimod=1	0	none
Process Parameters			
tox	Gate oxide thickness	1.50E-8	m
xj	Junction depth	1.50E-7	m
gamma1	Body-effect coefficient near the surface	0 (calculated)	$V^{1/2}$
gamma2	Body-effect coefficient in the bulk	0 (calculated)	$V^{1/2}$
nch	Channel doping concentration	1.7E17	$1/cm^3$
nsub	Substrate doping concentration	6.0E16	$1/cm^3$
vbx	Vbs at which the depletion region width=xt	0	V
xt	Doping depth	1.55E-7	m
Bound Parameters			
lmin	Minimum channel length	0	m
lmax	Maximum channel length	1	m
wmin	Minimum channel width	0	m
wmax	Maximum channel width	1	m
binunit	Bin unit selector	1	none

The BSIM3 model still retains the same basic physical properties of version 2.0. For example, effects like threshold voltage roll-off, non-uniform doping effect, mobility reduction due to vertical field, carrier velocity saturation, channel-length modulation, drain induced- barrier lowering, substrate current-induced body effect, subthreshold conduction, and parasitic resistance effects are all included. The BSIM3 version yields a more continuous behavior and facilitates faster convergence.

EPLF-EKV 2.6 LEVEL 9 MOSFET Model

The EPLF-EKV 2.6 LEVEL 9MOSFET model is scalable and compact for use in the design and simulation of low-voltage, low-current analog, and mixed analog-digital circuits using submicron CMOS technologies.

The EKV MOSFET model is built on fundamental physical properties of the MOS structure. It is formulated as a “single expression,” which preserves continuity of first- and higher-order derivatives with respect to any terminal voltage, in the entire range of validity of the model.

These physical effects are included in the 2.6 model version:

- Basic geometrical and process related aspects: oxide thickness, junction depth, effective channel length and width.
- Effects of doping profile and substrate effect.
- Modeling of weak, moderate and strong inversion behavior.
- Modeling of mobility effects due to vertical field.
- Short-channel effects for velocity saturation, channel-length modulation (CLM), source and drain charge-sharing (including for narrow channel widths), reverse short-channel effect (RSCE).
- Modeling of substrate current due to impact ionization.
- Quasistatic charge-based dynamic model.
- Thermal and flicker noise modeling.
- First-order non-quasistatic model for the transadmittances.
- Temperature effects.
- Short-distance geometry- and bias-dependent device matching.

The EKV model was developed by the Electronics Laboratories of the Swiss Federal Institute of Technology in Lausanne.

EPLF-EKV V. 2.6 LEVEL9 MOSFET MODEL

Symbols	Description	Default	Unit
Model Control Parameters			
af	Flicker noise exponent	1	--
bex	Mobility temperature exponent	-1.5	--
cbd	B-D p-n capacitance	0	F
cbs	B-S p-n capacitance	0	F
cgbo	Gate-bulk overlap capacitance	0	F
cgdo	Gate-drain overlap capacitance	0	F
cgso	Gate-source overlap capacitance	0	F
cj	Bottom p-n capacitance per area	0	F/m^2
cjsw	Sidewall p-n grading coefficient	0	F/m
cox	Gate oxide capacitance	0.0007	F/m^2
dl	Channel length correction	0	m
dw	Channel width correction	0	m
e0	New mobility reduction coefficient	1e+012	V/m
ekvint	Interpolation function selector	0	--
fc	Forward p-n capacitance coefficient	0.5	--
gamma	Body effect parameter	1	$\sqrt{V}$
iba	First impact ionization coefficient	0	1/m
ibb	Second impact ionization coefficient	3e+008	V/m
ibbt	Temperature coefficient for ibb	0.0009	1/k
ibn	Saturation voltage factor for impact ionization	1	--
is	Bulk p-n saturation current	1e-014	A
js	Bulk p-n bottom saturation current per area	0	A/m^2
jsw	Bulk p-n sidewall saturation current per length	0	A/m
kf	Flicker noise coefficient	0	--
kp	Transductance parameter	5e-005	A/V^2
lambda	Depletion length coefficient	0.5	--
leta	Short channel coefficient	0.1	--
lk	RSCE characteristic length	2.9e-007	m
mj	Forward p-n capacitance coefficient	0.5	--
mjsw	Sidewall p-n capacitance per length	0.33	F/m
n	Emission coefficient	1	--
nlevel	Noise level selector	1	--
nqs	Non-Quasi-Static operation switch	0	--
pb	Bulk p-n junction potential	0.8	V
pbsw	Bulk sidewall p-n junction potential	0.8	V
phi	Bulk Fermi potential	0.7	V
q0	RSCE excess charge	0	$A \bullet s / m^2$
rd	Drain ohmic resistance	0	Ω
rdc	Drain contact resistance	0	Ω

EPLF-EKV V. 2.6 LEVEL9 MOSFET MODEL			
Symbols Model	**Description Control Parameters**	**Default**	**Unit**
rs	Source ohmic resistance	0	Ω
rsc	Source contact resistance	0	Ω
rsh	Drain, source sheet resistance	0	Ω
satlim	Ratio defining the saturation limit	54.6	--
tcv	Threshold voltage temperature coefficient	0.001	V/K
theta	Mobility reduction coefficient	0	--
tnom	Parameter measurement temperature	27	°C
tr1	First order temperature coefficient	0	--
tr2	Second order temperature coefficient	0	--
tt	Bulk p-n transit time	0	sec
ucex	Longitudinal critical field temperature coefficient	0.8	--
ucrit	Longitudinal critical field	1e+008	V/m
vto	Nominal threshold voltage	0.5	V
weta	Narrow channel effect coefficient	0.25	--
xj	Junction depth	1e-007	m
xti	Junction current temperature exponent	3	--

BSIM 4 MODELS

The BSIM4 model parameters are listed in the BSIM4 manual included with the software and on the installation CD.

Fully-Depleted SOI MOS Model

The Fdsoi model is a new fully-depleted (FD) SOI MOSFET model. The model is charge conserving and presents an infinite order of continuity for all the small and large signal parameters. This is a very desirable property for a model to have and it is required in order to obtain good for a good performance in circuit analysis. The Fdsoi model is the first semiconductor model ever implemented as a C code (XDL) model. It is stored in SOIMOS.DLL in the IS directory.

This device has four terminals: front gate, back gate, source and drain. The FD SOI MOSFET has been proven to exhibit clear advantages over bulk MOSFETs, especially in low-power circuits [9-2]. The model consists of an intrinsic part and an

Fully-Depleted SOI MOSFET		
Name	**Description**	**Default**
w	channel width	2u
l	channel length	2u
tof	front oxide thickness	3.5n
tob	back oxide thickness	40n
tb	film thickness	8n
nsub	film doping	8e10
u0	zero-bias mobility	6e-2
temp	temperature	300
rd	drain/source resistance	0
nit	interface states charge	0
vthf	strong inversion threshold voltage	0.5
vthfi	weak inversion threshold voltage	0.5
af	mobility degradation parameter	1.5e-8
snt	weak/strong inversion smoothness	1
sigma	DIBL/DICE parameter	0
kappa	back bias parameter	-0.6
ld	charactersitic length	1e-7
qof	front oxide trapped charge	0
qob	back trapped charge density	0
ats	triode/saturation smoothness	6
vsat	saturation velocity	1e5
ldiff	diffusion length	0.0
llat	lateral diffusion length	0.0
wd	diffusion width	0.0
af1	Phonon scattering parameter	0.0
af2	surface roughness parameter	0.0
mob	mobility model option	0.0
ene	subthreshold slope	0.0
sat	velocity saturation model option	0.0
kv	temp. dependence of vsat	1.0
kaf	temp. dependence of af	1.0
kaf1	temp. dependence of af1	1.0
kaf2	temp. dependence of af2	1.0
kvth	temp. dependence of vthf	0.0
ca	control parameter	0.0
dvthl	vthf reduction on 1	0.0
dkap	kappa dependence on 1	0.0
dene	ene dependence on 1	1.0 (0 PMOS)
icgf	init. Vgf	0.1 (0 PMOS)
vfbf	front flat-band voltage	0
vfbb	back flat-band voltage	0
ics	init. vs	0 (5 PMOS)
icgb	init. vgb	0 (5 PMOS)
icd	init. vd	1 (3 PMOS, limit @ 10)
q0	inversion charge density at threshold	-0.2

extrinsic part. The intrinsic part is determined by the channel current (from source to drain) and the intrinsic charges at the four terminals, which are written as explicit continuous functions of bias. The effect of the parasitic drain-source resistance is included in the intrinsic model. The total charge expressions are obtained using the quasi-static approximation. The intrinsic capacitances are obtained by differentiation of the total charges with respect to the applied bias. The transient currents flowing into the terminals are expressed as time derivatives of the terminal charges. The extrinsic part of the model consists of the overlap and junction capacitances. References detailing the model are listed in Chapter 9 in the section dealing with the FD SOI MOS code model.

Subcircuits

A subcircuit that consists of IsSpice4 elements can be called and defined in a manner similar to device models. The subcircuit is defined in the input netlist by a group of element statements; IsSpice4 then automatically inserts the group of elements whenever the subcircuit is called. There is no limit to the size or complexity of subcircuits, and subcircuits may contain other subcircuits. Subcircuit calls may not be recursive.

Subcircuit Call Statement

IsSpice4 allows nested subcircuits.

Format: X*name N1* [*N2 N3* ...] *subname*

Examples: X1 1 2 3 4 5 OPAMP

Subcircuit calls begin with the letter X. Nodes are listed in the same order in which they are defined in the .SUBCKT statement, and refer to connections within the subcircuit. The subcircuit name, *subname*, is specified after the node list.

Subcircuit Connectivity Note: The order of the connections in the calling statement (X) must match the order of the connections in the subcircuit statement (.SUBCKT) exactly in terms of number and position. An error will result if the number

of connections are not equal. Incorrect simulation results will be generated if the order does not correspond, since the connections will be crossed. For example, node *N1* in the X line must be the same I/O point referrenced by node *N1* in the .SUBCKT line.

.Subckt Statement

Format: .SUBCKT *subnam N1* [*N2 N3* ...]

Examples: .SUBCKT OPAMP 1 2 3 4

Use the .OPTIONS LIST command to see the full IsSpice 4 netlist.

A subcircuit definition begins with a .SUBCKT line. *Subname* is the subcircuit name, and *N1*, *N2*, ... are the nodes referenced in the subcircuit that you want to connect to the calling (X) statement. Unlike in SPICE 2, node zero may be included on the .SUBCKT line, as well as on the (X) calling line.

The group of element lines, which immediately follow the .SUBCKT line, define the subcircuit. The last line in a subcircuit description must be the .ENDS statement. Control statements may not appear within a subcircuit definition; however, subcircuit definitions may contain anything else, including other subcircuit definitions, device models, and subcircuit calls. Note that any device models or subcircuit definitions that are included as part of a subcircuit definition are strictly local (i.e., such models and definitions can not be used outside of the subcircuit definition). Also, any element nodes that are not included on the .SUBCKT line are strictly local, with the exception of 0 (ground), which is always global.

When a circuit is parsed before simulation, all devices and local nodes in the subcircuit are renamed as:

device keyletter:X call name:ref-des name
X call name1:X call name 2:...:node

For example, a resistor (R1 1 0 1K) in the subcircuit XOP will be listed as “R:OP:1 1 0 1K”. Nodes in subcircuits are viewed the

same way. For example, .PRINT DC V(SUB:5) will print node 5 in the subcircuit called by XSUB. Nested subcircuit instances will have multiple qualifiers separated by colon. To see the "flattened" subcircuit listing, use the .OPTIONS LIST function. The complete netlist will appear in the IsSpice4 output file.

.Ends Statement

Format: .ENDS [*subname*]

Examples: .ENDS OPAMP

This line must be the last one in any subcircuit definition. The subcircuit name, if included, indicates which subcircuit definition is being terminated; if omitted, all subcircuits being defined are terminated. The name is required only when nested subcircuit definitions are being defined. Since subcircuits can be listed sequentially, with the same effect, it is not recommended that subcircuits be nested. For example,

Recommended	Not Recommended
.SUBCKT	.SUBCKT
.	
.ENDS	.SUBCKT
.SUBCKT	.SUBCKT
.	
.ENDS	.ENDS
.SUBCKT	.ENDS
.	
.ENDS	.ENDS

Code Model Syntax

Introduction

This chapter is divided into sections containing analog, hybrid (analog/real/digital interfaces), and digital code models. The syntax used here follows the same format as the previous chapter.

Format: A*name N1 N2 value*

Examples:
```
A1 [1  2] 3 nor
.model nor d_nor(....)
A1 1 2 Mygain
.model Mygain gain(...)
```

- All code models use the reference designation letter “A”.
- All code models require a .model statement
- Items in capital letters must appear exactly as shown.
- Items in italics must be replaced by user-defined data.

The relationship between the code model call line (i.e. A1 1 2 Mygain) and the .Model line (i.e. .Model Mygain gain(...)) is discussed in detail in the Device Model Statements section in the previous chapter. Since each code model requires a .Model statement, an example is provided after the call line.

In addition to syntax information, two tables are included for each model. The Port Table contains all the information about the input and output connections of the device. The Parameter table contains all of the information about the device’s model parameters.

The Port Table

The following list contains a brief explanation of the values in the Port Table. These entries completely describe the connections for a code model. Any entry that does not require a value will contain a hyphen "-".

Port Name
The internal name used to represent the port. This name is used only within the simulator and is not important for netlist construction.

Description
A brief text description of the purpose and function of the port.

Direction
The intended data flow direction of the port. The value will be; in for input only, out for output only, or inout for both input and/or output.

Default_Type
The default signal type that will be expected at the port. This can be one of the following:

Type	Description	Direction
d	digital	in or out
g	conductance (VCCS)	inout
gd	differential conductance (VCCS)	inout
h	resistance (CCVS)	inout
hd	differential resistance (CCVS)	inout
i	current	in or out
id	differential current	in or out
v	voltage	in or out
vd	differential voltage	in or out
vnam	voltage source name	in

Allowed_Types
The signal types that are allowed at the port. One or more of the values listed in the table above will be present.

Vector
This entry is either a “Yes” or “No”. No signifies a single connection. Yes means that a variable number of connections, similar to a bus, can be made to the port. If this value is YES, the vector bounds field will contain limits for the number of connections. A vector connection is identified by grouping the nodes within square braces such as [1 2 3 4]. An example call line for a NAND gate would look like:

A1 [1 2 3 4] 5 NAND
.MODEL NAND D_NAND(... *parameters* ...)

Vector_Bounds
The lower and upper limit on the number of connections that can be made if vector connections are allowed.

Null_Allowed
This entry is either a YES or NO. YES means the port may be left unconnected. NO means a connection is required. The string “NULL” is used as a placeholder on the call line. It replaces the node number and indicates an unconnected port.

The ports listed in the Port Table appear in the order required by the device’s call line. Referring to the Default_Type, Vector, and Vector_Bounds fields below, the device requires that the input is a digital vector with at least 2 nodes. Both input and output ports are required. For example, A1 [1 2] 3 ModName would be a valid call line.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

The Parameter Table

The following list contains an brief explanation of the values that are present in the Parameter table. These entries describe the parameters needed to create a .Model statement for a code model. The entries can appear in any order. Any entry that does not require a value will contain a hyphen "-".

Parameter_Name
The name of the parameter.

Description
A text description of the purpose and function of the parameter.

Data_Type
The type of value that the parameter will accept. Valid data types are boolean, complex, int, real, and string.

Default_Value
The default value used by the model if no value is entered. If Null_Allowed is YES, and there is no default value, the model parameter will not be used.

Limits
Specifies the limits for parameter values. A range of values is specified by enclosing the upper and lower limits in square braces separated by a space. For example, [2 10] would limit the model parameter to values between 2 and 10, inclusive. If the upper or lower bound is unconstrained then a hyphen is used. For example, [10 -] limits the parameter to all values greater than or equal to 10.

Vector
If this value is TRUE, or YES, then a vector (set of parameter values) is expected. A vector parameter may contain values separated by spaces, commas or parentheses, and must be enclosed in square braces. For example, den_array=[0 10 100] or cntrl_freq_array=[0,10k 1,20k 2,100k].

Vector_Bounds
This parameter specifies the limits for a vector model parameter. The first entry specifies the minimum number of values required.

Null_Allowed
A value of TRUE, or YES, means that the parameter can be left unstated. If it is set to FALSE, or NO, a value must be entered.

Analog Code Models

Analog code models operate using continuous voltages and currents like traditional SPICE models. Their inputs and outputs all use the analog node type. No special translational bridges are required to interconnect these elements unless a connection is being made to a real or digital node type. The following analog models are supplied with IsSPICE4.

The Vswitch model is also discussed in Chapter 8.

Model Type	Device
Core	Magnetic Core
D_dt	Time-derivative
Fdsoin/Fdsoip	Fully depleted SOI Mosfet N/P channel
Hyst	Hysteresis
Lcouple	Inductive coupling
Limit	Limiter
Oneshot	Controlled oneshot
Pwl	Table Model with slope extension
Pwl2	Table Model with limiting
S_xfer	s-domain transfer function
Slew	Slew rate follower
Sine	Controlled sine wave oscillator
Square	Controlled square wave oscillator
Triangle	Controlled triangle wave oscillator
Vsrc_pwl	Repeating piece-wise linear source
Vswitch	Smooth transition Switch

Magnetic Core

Format: A*name (plus minus) modname*
.Model *modname* core(pn1=*pv1* pn2=*pv2*..)

Example: A2 (3 4) iron_core
.Model iron_core core(area = 0.01 length = 0.01
+ hb_array = [-1000 -1000...)]...)

This model is used as a building block to create a wide variety of magnetic circuit models. This function is normally used in conjunction with the inductive coupling model (lcouple) to build systems that emulate the behavior of linear and nonlinear magnetic components. There are two fundamental modes of operation for this magnetic core model; the pwl mode and the hysteresis mode. The default is pwl mode.

PWL Mode (mode = 1)
The core model in PWL mode takes a voltage input that it treats as a magnetomotive force (mmf) value. This value is divided by the total effective length (length model parameter) of the core to produce a value for the magnetic field Intensity, H. This value of H is then used to find the corresponding flux density, B, using the piecewise linear relationship described by the HB_array data pairs. B is then multiplied by the cross-sectional area (area model parameter) of the core to find the flux value. The flux is then output as a current. The pertinent mathematical equations are listed below:

H = mmf/L, where L=length and H=ampere-turns/meter

The B value is derived from a piecewise linear transfer function described to the model via the HB_array data pairs. This transfer function DOES NOT include hysteretic effects.

The final current allowed to flow through the core is equal to **Φ**.

Φ =BA, where A=area

This value is in turn used by an Lcouple model to obtain a value for the voltage, which is reflected back across its terminals to the driving electrical circuit.

The following example netlist shows the use of two Lcouple models and one core model to produce a simple primary/ secondary transformer.

```
A1 (2 0) (3 0) primary
.Model primary lcouple (num_turns = 155)
A2 (3 4) iron_core
.Model iron_core core (HB_array = [-1000,-3.13M -500,-2.63M -375,-2.33M
+ -250,-1.93M -188,-1.5M -125,-.625M -63,-.25M 0,0 63,.25M 125,.625M
+ 188,1.5M 250,1.93M 375,2.33M 500,2.63M 1000,3.13M] area = 0.01
+ length = 0.01)
A3 (5 0) (4 0) secondary
.Model secondary lcouple (num_turns = 310)
```

HYSTERESIS Mode (mode = 2)

The core model in hysteresis mode takes as an input a voltage, which it treats as a magnetomotive force (mmf) value. This value is used as an input to the equivalent of a hysteresis code model block. The parameters defining the input low and high values, the output low and high values, and the amount of hysteresis are as defined in the hysteresis model. The output from this mode, as in PWL mode, is a current value that is seen across the core. An example of the core model used in this fashion is shown below:

```
 A1 (2 0) (3 0) primary
.Model primary lcouple (num_turns = 155)
A2 (3 4) iron_core
.Model iron_core core (mode = 2 in_low=-7.0 in_high=7.0
+ out_lower_limit=-2.5e-4 out_upper_limit=2.5e-4 hyst = 2.3 )
A3 (5 0) (4 0) secondary
.Model secondary lcouple (num_turns = 310)
```

One final note about the two core models: certain parameters are available in one mode, but not in the other. The in_low, out_lower_limit, out_upper_limit, and hysteresis parameters are not available in PWL mode. The HB_array, area, and length parameters are not available in Hysteresis mode. The input_domain and fraction parameters are common to both

modes although their behavior is somewhat different. For an explanation of the input_domain and fraction values for Hysteresis mode, please refer to the hysteresis (HYST) code model discussion.

Port Table

Port_Name:	mc
Description:	“magnetic core”
Direction:	inout
Default_Type:	gd
Allowed_Types:	[g,gd]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	no

Parameter Table

Parameter_Name:	HB_array
Description:	“field-flux desity array”
Data_Type:	real
Default_Value:	-
Limits:	-
Vector:	yes
Vector_Bounds:	[2 -]
Null_Allowed:	no

Parameter_Name:	area	length
Description:	“cross-sectional area”	“core length”
Data_Type:	real	real
Default_Value:	-	-
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter_Name:	input_domain	fraction
Description:	“input sm. domain”	“smoothing switch”
Data_Type:	real	boolean
Default_Value:	0.01	TRUE
Limits:	[1e-12 0.5]	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	mode
Description:	“mode switch (1 = pwl, 2 = hyst)”
Data_Type:	int
Default_Value:	1
Limits:	[1 2]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Parameter_Name:	in_low	in_high
Description:	“input low value”	“input high value”
Data_Type:	real	real
Default_Value:	0.0	1.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	hyst	out_lower_limit	out_upper_limit
Description:	“hysteresis”	“output lower limit”	“output upper limit”
Data_Type:	real	real	real
Default_Value:	0.1	0.0	1.0
Limits:	[0 -]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Differentiator

Format: A*name Input Output modname*
.Model *modname* d_dt(pn1=*pv1*)

Example: A12 7 12 slope_gen
.Model slope_gen d_dt(out_offset=0.0 gain=1.0
+ out_lower_limit=1e-12 out_upper_limit=1e12
+ limit_range=1e-9)

The differentiator block is a simple derivative stage that approximates the time derivative of an input signal by calculating the incremental slope of the input since the previous timepoint. The block also includes gain and offset parameters to allow for tailoring of the required signal, and output upper and lower limits to prevent convergence errors resulting from excessively large output values. The incremental value of output below the output_upper_limit and above the output_lower_limit at which smoothing begins is specified via the limit_range parameter.

Note: In the AC analysis, the value returned is equal to the radian frequency of analysis multiplied by the gain. It is not recommended that the model be used to provide integration through the use of a feedback loop. The Laplace code model can be used to provide the integration function (1/s).

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	gain	out_offset
Description:	“gain”	“output offset”
Data_Type:	real	real
Default_Value:	1.0	0.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	out_lower_limit	out_upper_limit
Description:	“output lower limit”	“output upper limit”
Data_Type:	real	real
Default_Value:	-	-
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	limit_range
Description:	“smoothing limit range”
Data_Type:	real
Default_Value:	1.0e-6
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Fully Depleted SOI Mosfet

Format: A*name Drain Gate Source BackGate modname*
.Model *modname* fdsoin (pn1=*pv1*) - NMOS
.Model *modname* fdsoip (pn1=*pv1*) - PMOS

Example: A1 1 2 3 4 Fdsoin
.MODEL Fdsoin Fdsoin(w=5e-6 l=5e-6 tof=34e-9 tob=450e-9
+ tb=75e-9 nsub=8e22 u0=6.1e-2 temp=298 rd=0 nit=0
+ vthf=0.8 vthfi=0.8 af=1e-8 snt=1 q0=0 sigma=0
+ kappa=3.2e-2 ld=0.9e-7 qof=0 qob=0 ats=6 vsat=1e5
+ ldiff = 4e-6 llat=0.3e-6 wd=0.5e-6 icgf=4 vfbf=0 vfbb=0
+ ics=0 icgb=0 q0=0)

The Fdsoi models represent a new fully-depleted (FD) SOI MOSFET (NMOS and PMOS versions). The model is charge conserving and presents an infinite order of continuity for all the small and large signal parameters.

This device has four terminals: front gate, back gate, source and drain. The FD SOI MOSFET has been proven to exhibit clear advantages over bulk MOSFETs, especially in low-power circuits [9-2]. The model consists of an intrinsic part and an extrinsic part. The intrinsic part is determined by the channel current (from source to drain) and the intrinsic charges at the four terminals, which are written as explicit continuous functions of bias. The effect of the parasitic drain-source resistance is included in the intrinsic model. The total charge expressions are obtained using the quasi-static approximation. The intrinsic capacitances are obtained by differentiation of the total charges with respect to the applied bias. The transient currents flowing into the terminals are expressed as time derivatives of the terminal charges. The extrinsic part of the model consists of the overlap and junction capacitances.

[9-1] J. -P. Colinge, Silicon-on-Insulator Technology: Materials to VLSI, Norwell, MA: Kluwer,

[9-2] J. P. Colinge, J. P. Eggermont, D. Flandre, P. Francis and P. Jespers. “Potential of SOI for analog and mixed analog-digital low-power applications”, Proc. ISSCC’95, pp. 194-195, February 1995.
[9-3] B. Iniguez, L. F. Ferreira, B. Gentinne and D. Flandre, “A Physically-Based Continuous Fully-Depleted SOI MOSFET Model for Analog Applications”, IEEE Trans. on Electron Devices, vol. 43, no. 4, April 1996.

Port Table

Port_Name:	drain	fgate	source	bgate
Description:	“drain”	“front gate”	“source”	“back gate”
Direction:	inout	inout	inout	inout
Default_Type:	g	g	g	g
Allowed_Types:	[g v i]	[g,v,i]	[g,v,i]	[g,v,i]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	no	no	no	no

PARAMETER_TABLE:

Parameter_Name:	w	l	tof	tob
Description:	“width”	“length”	“front oxide tk.”	“back oxide tk.”
Data_Type:	real	real	real	real
Default_Value:	2e-6	2e-6	3.5e-9	40e-9
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	tb	nsub	u0	temp
Description:	“film tk.”	“film doping”	“zero-bias mob.”	“temp”
Data_Type:	real	real	real	real
Default_Value:	8e-9	8e10	6e-2	300
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	vfbf	vfbb	rd	nit
Description:	“front f-b voltage”	“back f-b volt.”	“drain/src res”	“int. states charge”
Data_Type:	real	real	real	real
Default_Value:	0	0	0	0
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	vthf	vthfi	vsat	af
Description:	“sinv. th. volt.”	“weak inv. th. volt.”	“satuation vel.”	“mobility degradation”
Data_Type:	real	real	real	real
Default_Value:	0.5	0.5	1e5	1.5e-8
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	snt	ats	sigma	kappa
Description:	“w/sinv. smoth”	“triode/sat. smooth”	“DIBL/DICE”	“back bias”
Data_Type:	real	real	real	real
Default_Value:	1	6	0	-0.6
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	ld	qof	qob	q0
Description:	“ch. length”	“ft. oxide trap cd”	“bk trapped cd”	“inv. charge density at th.”
Data_Type:	real	real	real	real
Default_Value:	1e-7	0	0	-0.2
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	icgf	icgb	icd	ics
Description:	“init. vgf”	“init. vgb”	“init. vd”	“init. vs”
Data_Type:	real	real	real	real
Default_Value:	0.1	0.0	1	0
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	llat	ldiff	wd
Description:	“lat. diff. len.”	“diff. length”	“diff. width”
Data_Type:	real	real	real
Default_Value:	0.0	0.0	0
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	af1	af2	mob
Description:	“phonon scat. parm”	“surf. rough parm”	“mobility model option”
Data_Type:	real	real	int
Default_Value:	0.0	0.0	0
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	ene	sat	ca	sigmal
Description:	“subth. slope”	“velocity saturation”	“control parm.”	“sigma dep. on l”
Data_Type:	real	int	int	real
Default_Value:	0.0	0	0	0
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	kv	kaf	kaf1	kaf2
Description:	“temp. dep. of vsat”	“temp dep. of kaf”	“temp. dep. of af1”	“temp. dep. of af2”
Data_Type:	real	real	real	real
Default_Value:	1.0	1.0	1.0	1.0
Limits:	-	-		- -
Vector:	no	no	no	no
Vector_Bounds:	-	-		- -
Null_Allowed:	yes	yes	yes	yes

PARAMETER_TABLE:

Parameter_Name:	kvth	dvthl	dkap	dene
Description:	“temp. dep. of vthf”	“vthf red. on l”	“kappa dep. on l”	“ene dep. on l”
Data_Type:	real	real	real	real
Default_Value:	0.0	0	0	0
Limits:	-	-	-	-
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

Note: See the SOI Mosfet syntax in Chapter 8 for a more complete description of each model parameter name.

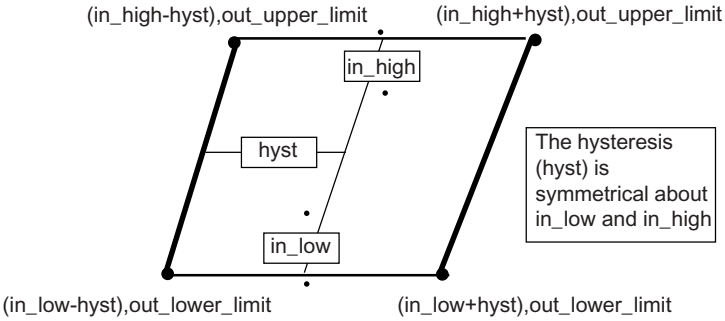
Hysteresis Block

Format: A*name Input Output modname*
.Model *modname* hyst(pn1=*pv1*)

Example:
```
A11 1 2 schmitt1
.Model schmitt1 hyst(in_low=0.7  in_high=2.4
+ hyst=0.5 out_lower_limit=0.5
+ out_upper_limit=3.0
+ input_domain=0.01  fraction=TRUE)
```

The hysteresis block is a simple buffer stage that provides hysteresis of the output with respect to the input. The in_low and in_high parameter values specify the center voltage or current about which the hysteresis effect operates. The output values are limited to out_lower_limit and out_upper_limit.

The value of the model parameter hyst is added to the in_low and in_high points in order to specify the points at which the slope of the hysteresis function would normally change abruptly as the input transitions from a low to a high value. Likewise, the value of hyst is subtracted from the in_high and in_low values in order to specify the points at which the slope of the hysteresis function would normally change abruptly as the input transitions from a high to a low value. Input_domain defines the increment below and above the corner points within, in which smoothing of the d(out)/d(in) values occur. This prevents abrupt changes in d(out)/d(in), which prevents convergence problems.



This figure represents the input/output hysteresis loop created by the hyst code model.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	in_low	in_high
Description:	“input low value”	“input high value”
Data_Type:	real	real
Default_Value:	0.0	1.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	hyst	out_lower_limit
Description:	“hysteresis”	“output lower limit”
Data_Type:	real	real
Default_Value:	0.1	0.0
Limits:	[0.0 -]	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	out_upper_limit	input_domain
Description:	“output upper limit”	“input smoothing domain”
Data_Type:	real	real
Default_Value:	1.0	0.01
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	fraction
Description:	“smoothing switch”
Data_Type:	boolean
Default_Value:	TRUE
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Inductive Coupling

Format: A*name (Input Nodes N1 N2)*
+ *(Output Nodes N3 N4) modname*
.Model *modname* lcouple(pn1=*pv1*)

Example: A150 (7 0) (9 10) lcouple1
.Model lcouple1 lcouple(num_turns=10.0)

This model is used as a building block to create a wide variety of inductive and magnetic circuit models. This function is normally used in conjunction with the magnetic core model, but can also be used with resistors, hysteresis blocks, etc. to build systems that emulate the behavior of linear and nonlinear components.

This model takes a current as the input to port L (input nodes N1 N2). This current value is multiplied by the num_turns value to produce an output voltage representing the magnetomotive force. When Lcouple is connected to the magnetic core model, or to a resistive device, a current will flow. This current value, which is modulated by whatever Lcouple is connected to, is used by Lcouple to calculate a voltage “seen” at the input. The voltage is a function of the derivative with respect to time of the current value seen at the output port, mmf_out.

The most common use for Lcouple is as a building block of transformer models. To create a transformer with a single input and a single output, you would use two Lcouple models plus one core model. See the Magnetic Core model for more information.

Port Table

Port_Name:	L	mmf_out
Description:	“inductor”	“mmf output (in ampere-turns)”
Direction:	inout	inout
Default_Type:	hd	hd
Allowed_Types:	[h,hd]	[hd]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	num_turns
Description:	“number of inductor turns”
Data_Type:	real
Default_Value:	1.0
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Limiter

Format: A*name Input Output modname*
.Model *modname* limit(pn1=*pv1* pn2=*pv2*..)

Example:
```
A5 1 2 limit5
.Model limit5 limit( in_offset=0.1  gain=2.0
+ out_lower_limit=-1.0 out_upper_limit=1.0
+ limit_range=0.10 fraction=FALSE)
```

The Limiter is a single input, single output function similar to the gain block. However, the output of the Limiter function is restricted to the range specified by the out_lower and out_upper limits. This model will operate in DC, AC and Transient analysis modes.

The linear range of the output is BELOW (out_upper_limit - limit_range) and ABOVE (out_lower_limit + limit_range). In this range, the output = gain * (in_offset + input). Smoothing of the output begins in the regions between the bounds of the linear range and the upper and lower limits defined in the model. If fraction is FALSE, then the limit_range value is interpreted as an absolute value. If fraction is TRUE, the limit_range is given by: limit_range = limit_range * (out_upper_limit - out_lower_limit).

For the example above, the output will begin to smooth out at ±0.9 volts.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	in_offset	gain	out_lower_limit
Description:	“input offset”	“gain”	“output lower limit”
Data_Type:	real	real	real
Default_Value:	0.0	1.0	0.0
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	limit_range	out_upper_limit
Description:	“smoothing limit range”	“output upper limit”
Data_Type:	real	real
Default_Value:	1.0e-6	1.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	fraction
Description:	“smoothing switch”
Data_Type:	boolean
Default_Value:	FALSE
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Controlled One-Shot

If the input is between two points in the cntl_pw_array, the output pulse width is determined by the linear interpolation between the two input points.

See the Table Model for more information.

Format: A*name Clk Control_Input Clear Output modname*
.Model *modname* oneshot(pn1=*pv1* pn2=*pv2*..)

Example: Ain 1 2 3 4 one
.Model one oneshot(out_low = 0 out_high = 4.5 duty_cycle = .9
+ cntl_pw_array = [-1,1U 0,1U 10,.1M 11,.1M] clk_trig = 0.9
+ pos_edge_trig = False rise_delay = 20N fall_delay = 35N)

The one-shot takes an input voltage, or current, as the independent variable in the piecewise linear curve described by the coordinate points of the cntl_pw_array parameters. From the curve, a pulse width is determined, and the oscillator will output a pulse of that width. The pulse will be delayed by the delay value and have the specified output values and rise and fall times. If the model parameter pos_edge_trig is TRUE (default), the one-shot is triggered by a rising clock edge at the value of clk_trig. If pos_edge_trig is FALSE, the one-shot will be triggered on the falling edge. The retrig parameter specifies whether or not the one-shot can be retriggered. By default, the oneshot cannot be retriggered. Set the retrig parameter to TRUE in order to retrigger this oneshot.

Port Table

Port Name:	clk	cntl_in
Description:	“clock input”	“control input”
Direction:	in	in
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id,vnam]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	yes

Port Name:	clear	out
Description:	“clear signal”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	no

Parameter Table

Parameter_Name:	clk_trig	pos_edge_trig
Description:	“clock trigger value”	“pos/neg edge trigger switch”
Data_Type:	real	boolean
Default_Value:	0.5	TRUE
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter_Name:	cntl_pw_array	out_low	out_high
Description:	“control/pw array”	“output low value”	“output high value”
Data_Type:	real	real	real
Default_Value:	-	0.0	1.0
Limits:	-	-	-
Vector:	yes	no	no
Vector_Bounds:	[2 -]	-	-
Null_Allowed:	no	yes	yes

Parameter_Name:	rise_delay	rise_time
Description:	“delay from trig.”	“output rise time”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	fall_delay	fall_time	retrig
Description:	“delay from pw”	“output fall time”	“retrigger switch”
Data_Type:	real	real	boolean
Default_Value:	1.0e-9	1.0e-9	FALSE
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

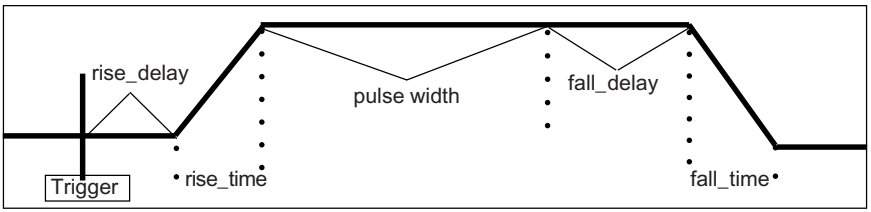


Table Models

Table Model With Slope Extension

Format: A*name Input Output modname*
.Model *modname* pwl(pn1=*pv1* pn2=*pv2*..)

Example:
```
A7 2 4 xfer_cntl1
.Model xfer_cntl1 pwl( xy_array=[-2.0 -0.2 -1.0
+ 0.2 2.0 0.1 4.0 2.0 5.0 10.0] input_domain=0.05
+ fraction=TRUE)
```

Table Model With Limiting

Format: A*name Input Output modname*
.Model *modname* pwl2(pn1=*pv1* pn2=*pv2*..)

Example:
```
A7 2 4 table2
.Model table2 pwl2( xy_array=[-1 -1  0 0
+ 1 1] input_domain=0.1
+ fraction=FALSE)
```

The table models (or piece-wise linear controlled sources) are single-input, single-output functions similar to the gain block. However, the output of the table models are not necessarily linear for all input values. Instead, they follow an I/O relationship specified via the xy_array coordinates in their .Model statement. The model name for the table model with slope extension is PWL. The model name for the table model with limiting is PWL2.

The xy_array values represent coordinate points on the x and y axes, respectively. There may be as few as two pairs specified, or as many pairs as memory and simulation speed

allow. This permits you to approximate a nonlinear function by entering multiple input-output coordinate points.

Two aspects of the table model warrant special attention. These are the handling of endpoints and the smoothing of the described transfer function near coordinate points.

In order to produce output for input values outside of the bounds of the PWL function, the table model extends the slope found between the lowest two coordinate pairs and the highest two coordinate pairs. This has the effect of making the transfer function completely linear for an input less than xy_array[0,0] and greater than xy_array[n,n]. It also has the potentially subtle effect of unrealistically causing an output to reach a very large or small value for large inputs.

Note: The PWL table model does not inherently provide a limiting capability. PWL2, which has limiting, can be used if limiting outside the table value range is desired.

For output values corresponding to input values outside of the bounds of the PWL2 function, the table model limits the output value to the endpoint values (0 value slope) found below the lowest coordinate pair and above the highest coordinate pair. This has the effect of limiting the transfer function output inputs less than xy_array[0,0] and greater than xy_array[n,n].

In order to diminish the potential for nonconvergence when using the PWL block, a form of smoothing around the xy_array coordinate points is necessary. This is due to the iterative nature of the simulator and its reliance on smooth first derivatives of transfer functions in order to arrive at a matrix solution. Consequently, the “input_domain” and “fraction” parameters

are included to provide some control over the amount and nature of the smoothing performed.

“Fraction” is a switch that is either TRUE or FALSE. When TRUE, the simulator assumes that the specified input_domain value is to be interpreted as a fractional figure. Otherwise, it is interpreted as an absolute value. Thus, if fraction is TRUE and input_domain=0.10, the simulator assumes that the smoothing radius about each coordinate point is equal to 10% of the length of either the x array segment above each coordinate point, or the x array segment below each coordinate point. The specific segment length chosen will be the smallest of these two for each coordinate point. If fraction is FALSE and input=0.10, the simulator will begin smoothing the transfer function at 0.10V (or amperes) below each x array coordinate, and will continue the smoothing process for another 0.10 volts (or amperes) above each x array coordinate point. Since overlap of smoothing domains is not allowed, the model checks to ensure that the specified input_domain value is not excessive.

One subtle consequence of the use of the fraction=TRUE feature of the table model is that, in certain cases, you may inadvertently create extreme smoothing of functions by choosing inappropriate coordinate value points. This can be demonstrated by considering a function described by three coordinate pairs, such as (-1,-1), (1,1), and (2,1). In this case, with a 10% input_domain=0.10), you would expect to see rounding to occur between in=0.9 and in=1.1, and nowhere else. On the other hand, if you were to specify the same function using the coordinate pairs (-100,-100), (1,1) and (201,1), you would find that rounding occurs between in=-19 and in=21. Clearly in the latter case, the smoothing might cause an excessive divergence from the intended linearity above and below in=1.

Using Table Models From Other SPICE Programs
Other SPICE programs may use a similar format for table-type models. If the data points are in an X,Y sequence you can simply:

- Select and copy the points from the existing netlist in any text editor.
- Then edit the SPICE model library file containing the table code model or the Properties dialog for the table code model.
- You can paste in the data points into the xy_array model parameter field.

Port Table

Port_Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	xy_array	
Description:	“xy-element array”	
Data_Type:	real	
Default_Value:	-	
Limits:	-	
Vector:	yes	
Vector_Bounds:	[2 -]	
Null_Allowed:	no	

Parameter_Name:	input_domain	fraction
Description:	“input sm. domain”	“smoothing switch”
Data_Type:	real	boolean
Default_Value:	0.01	TRUE
Limits:	[1e-12 0.5]	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Laplace (s-Domain) Transfer Function

Format: A*name Input Output modname*
.Model *modname* s_xfer(pn1=*pv1* pn2=*pv2*..)

Example:
```
A12 1 2 Cheby3K
.Model Cheby3K  s_xfer(in_offset=0.0
+ gain=1.0   num_coeff=[1.0]
+ den_coeff=[1.0 1.42562 1.51620])
```

The s-domain transfer function is a single-input, single-output Laplace transfer function that provides flexible modeling of the frequency-domain characteristics of a signal. The code model may be configured to produce an arbitrary s-domain transfer function with the following restrictions:

- The degree of the numerator polynomial cannot exceed that of the denominator polynomial in the variable “s”.
- The coefficients for a polynomial must be stated explicitly. That is, if a coefficient is zero, it must be included as an input to the num_coeff or den_coeff vector.
- Only scientific notation is allowed for the coefficients. In other words, 3.578*10^13 should be entered as 3.578e13.

The order of the coefficient parameters is from the highest-powered term, decreasing to the lowest. Thus, for the coefficient parameters specified below, the equation in “s” is shown:

```
.Model filter s_xfer(gain=0.139713 num_coeff=[1 0  0.074641]
+ den_coeff=[1   0.99894   0.011701])
```

...specifies a transfer function of the form...

$$0.13971 \bullet \frac{s^2 + .074641}{s^2 + 0.99894s + 0.011701}$$

The s-domain transfer function includes gain and input offset parameters that allow tailoring of the required signal. There are no limits on the internal signal values or on the output value of

the s-domain transfer function, so you are cautioned to specify gain and coefficient values that will not cause the model to produce excessively large values.

The denorm_freq term allows you to specify coefficients for a normalized filter (i.e., one in which the frequency of interest is 1 rad/s). Once these coefficients are included, specifying the denormalized frequency value "shifts" the corner frequency to the actual one of interest. As an example, the following transfer function describes a Chebyshev lowpass filter with a corner (passband) frequency of 1 rad/s:

$$\frac{1}{s^2 + 1.09773s + 1.10251}$$

In order to define an s_xfer model for the above equation, but with the corner frequency equal to 1500 rad/s (9425 Hz), the following model line will be needed:

```
.Model cheby1 s_xfer(num_coeff=[1]
+ den_coeff=[1 1.09773 1.10251] denorm_freq=1500)
```

Similar results could have been achieved by performing the denormalization prior to specification of the coefficients, and setting denorm_freq to a value of 1.0 (or not specifying the frequency, since the default is 1.0 rad/s). Note that frequencies are always specified in RADIANS/SECOND.

Port Table

Port Name:	in	out
Description:	"input"	"output"
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	in_offset	gain	num_coeff
Description:	“input offset”	“gain”	“numerator coeff”
Data_Type:	real	real	real
Default_Value:	0.0	1.0	-
Limits:	-	-	-
Vector:	no	no	yes
Vector_Bounds:	-	-	[1 -]
Null_Allowed:	yes	yes	no

Parameter_Name:	den_coeff	out_ic
Description:	“denominator coeff”	“output initial value”
Data_Type:	real	real
Default_Value:	-	-
Limits:	-	-
Vector:	yes	no
Vector_Bounds:	[1 -]	-
Null_Allowed:	no	yes

Parameter_Name:	denorm_freq
Description:	“denormalized corner freq.(radians)”
Data_Type:	real
Default_Value:	1.0
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Slew Rate Block

Format: A*name Input Output modname*
.Model *modname* slew(pn1=*pv1* pn2=*pv2*..)

Example: A15 1 2 slew1
.Model slew1 slew(rise_slope=0.5U
+ fall_slope=1U)

For more detail on the piecewise linear response, see the Table code model.

This function is a simple slew rate block that limits the absolute slope of the output with respect to time. The actual slew rate effects of over-driving an amplifier circuit can be accurately modeled by cascading the amplifier with this model. The units used to describe the maximum rising and falling slope values are expressed in volts, or amperes, per second. Thus a desired slew rate of 0.5 V/µs will be expressed as 0.5e+6, etc.

The slew rate block will continue to raise or lower its output until the difference between the input and the output values are zero. Thereafter, it will resume following the input signal, unless the slope again exceeds its rise or fall slope limits. The range input specifies a smoothing region above or below the input value. Whenever the model is slewing and the output comes to within the input + or - the range value, the partial derivative of the output with respect to the input will begin to smoothly transition from 0.0 to 1.0. When the model is no longer slewing (output = input), dout/din will equal 1.0.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_slope	fall_slope
Description:	“max rising slope”	“max falling slope”
Data_Type:	real	real
Default_Value:	1.0e9	1.0e9
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Controlled Sine Wave Oscillator

Format: A*name Control_Input Output modname*
.Model *modname* sine(pn1=*pv1* pn2=*pv2*..)

Example: Asine 1 2 in_sine
.Model in_sine sine(out_low = -5 out_high = 5
+ cntl_freq_array = [-1,10 0,10 5,1K 6,1K])

The controlled sine wave oscillator takes an input voltage, or current value, and uses it as the independent variable in the piecewise linear curve described by the coordinate points of the cntl_freq_array model parameter. From the curve and the input signal, a frequency value is determined, and the oscillator will output a sine wave at that frequency with peak values described by out_low and out_high. If the input is between two points in the cntl_freq_array, the output frequency is determined by the linear interpolation between the two points.

The cntl_freq_array values represent coordinate points on the x and y axes, and normally represent voltage and frequency pairings. There may be as few as two pairs specified, or as many as memory and simulation speed allow. This permits you to accurately approximate a nonlinear function of frequency by entering multiple input-output coordinate points.

Cntl_freq_arrays with 2 x, y points will yield a linear variation of frequency with respect to the control input. Greater array sizes will yield a piecewise linear response.

Port Table

Port Name:	cntl_in	out
Description:	“control input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	cntl_freq_array	
Description:	“control/freq array”	
Data_Type:	real	
Default_Value:	0.0	
Limits:	-	
Vector:	yes	
Vector_Bounds:	[2 -]	
Null_Allowed:	no	

Parameter_Name:	out_low	out_high
Description:	“peak low value”	“peak high value”
Data_Type:	real	real
Default_Value:	-1.0	1.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Controlled Square Wave Oscillator

Format: A*name Control_Input Output modname*
.Model *modname* square(pn1=*pv1* pn2=*pv2*..)

Example:
```
Ain 1 2 pul
.Model pul square(out_low = 0 out_high = 4.5
+ cntl_freq_array = [-1,10  0,10  5,1K  6,1K]
+ rise_time = 1U fall_time = 2U
+ duty_cycle = 0.2)
```

The controlled square wave oscillator is characterized by the values of out_low, out_high, duty_cycle, rise_time, and fall_time. It takes an input voltage, or current, and uses it as the independent variable in the piecewise linear curve, which is described by the coordinate points of the cntl_freq_array parameter. The oscillator will output a square wave at the frequency described by the curve and the input signal. If the input is between two points in the cntl_freq_array, the output frequency is determined by the linear interpolation between the two points. The cntl_freq_array values represent coordinate points on the x and y axes, respectively, and normally represent voltage and frequency, or current and frequency pairings.

Port Table

Port Name:	cntl_in	out
Description:	“control input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id, vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	cntl_freq_array
Description:	“control/freq array”
Data_Type:	real
Default_Value:	-
Limits:	-
Vector:	yes
Vector_Bounds:	[2 -]
Null_Allowed:	no

Parameter_Name:	out_low	out_high
Description:	“peak low value”	“peak high value”
Data_Type:	real	real
Default_Value:	-1.0	1.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	duty_cycle	rise_time	fall_time
Description:	“duty cycle”	“rise time”	“fall time”
Data_Type:	real	real	real
Default_Value:	0.5	1.0e-9	1.0e-9
Limits:	[1e-6 0.999999]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Controlled Triangle Wave Oscillator

Format: A*name Control_Input Output modname*
.Model *modname* triangle(pn1=*pv1* pn2=*pv2*..)

Example:
```
Ain 1 2 ramp
.Model ramp triangle(out_low = -5 out_high = 5.0
+ cntl_freq_array = [-1,10  0,10  5,1K  6,1K]
+ duty_cycle = 0.9)
```

The controlled triangle wave oscillator is characterized by the values out_low, out_high and rise_duty. Its input is either a voltage or current. This value is used as the independent variable in the piecewise linear curve described by the coordinate points of the cntl_freq_array parameter. The cntl_freq_array values represent coordinate points on the x and y axes, respectively, and normally represent voltage and frequency, or current and frequency pairings. From an input signal and the curve, a frequency value is determined, and the oscillator will output a triangle wave at that frequency. If the input is between two points in the cntl_freq_array, the output frequency is determined via linear interpolation between the two points.

Port Table

Port Name:	cntl_in	out
Description:	“control input”	“output”
Direction:	in	out
Default_Type:	v	v
Allowed_Types:	[v,vd,i,id,vnam]	[v,vd,i,id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	cntl_freq_array	duty_cycle
Description:	“control/freq array”	“rise time duty cycle”
Data_Type:	real	real
Default_Value:	-	0.5
Limits:	-	[1e-6 0.999999]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	yes

Parameter_Name:	out_low	out_high
Description:	“peak low value”	“peak high value”
Data_Type:	real	real
Default_Value:	-1.0	1.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Smooth Transition Switch

Format: A*name Output Nodes N1 N2*
+ Input_Controlling_Nodes N3 N4 modname
.Model modname vswitch(pn1=pv1...)

Example: Atest1 1 2 sw1
.Model sw1 vswitch(ron=1 roff=1meg)

The model provides a voltage controlled impedance with a smooth (continuous derivatives) transition region between the on and off states. The on and off impedances are defined by ron and roff respectively.

Port Table

Port_Name:	out	in
Description:	“output”	“input”
Direction:	inout	inout
Default_Type:	gd	gd
Allowed_Types:	[gd]	[gd]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	ron	roff
Description:	“on resistance”	“off resistance”
Data_Type:	real	real
Default_Value:	1.0	1.0e6
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	von	voff
Description:	“on voltage”	“off voltage”
Data_Type:	real	real
Default_Value:	1.0	0.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Repeating Piece-Wise Linear Source

Format: A*name Output N1 modname*
.Model modname vsrc_pwl(pn1=pv1...)

Example: Atest1 1 2 vsrc
.MODEL vsrc vsrc_pwl(
+ input_file=C:\User\Long.txt repeat=False)
.MODEL vsrc vsrc_pwl(input_file=mine.txt)

This code model reads a file containing piece-wise linear data point pairs and outputs the data as a voltage or current (two versions, one with voltage output and one with current output are included in ICAP/4). The data file is defined by the input_file parameter. The "repeat" parameter allows you to repeat the data stream (if it equals True", default case) for the duration of the transient analysis. A repeat value of "False" causes the pwl values to be run once. The model type is defined as vsrc_pwl.

PWL file Format/Definition
The pwl file has the following format/definition:

The pwl file can be located anywhere. The filename can have any extension. All text on a single line, following an * (asterisk) or ; (semicolon), is considered a comment. Each line is read separately and is trimmed of white spaces and + symbols before the data point reading begins.

The following search scheme is employed for the pwl file:

- Where the code model tells it to, i.e. the path stated in the input_file model parameter.
- In the working directory, i.e. the location of the .ckt or .cir file being simulated.
- In the directory pointed to by *ICAPSDir*\pr, where *ICAPSDir* is the ICAPS environment variable.
- In the directory pointed to by IS@@@, where IS@@@ is the network environment variable.
- In the directory where Spice4.Exe (IsSpice4) is located.

Note: this is the same search scheme use by all code models that access text files.

White spaces are defined as spaces, commas, tabs, and left and right parentheses. Data points must be in time, value pairs. These pairs must be consecutive from the top of the file to the bottom, i.e. time must increase monotonically.

Comment Characters
Comment characters can be overridden using the following syntax:

[Comment chars] "*;"

This statement can appear anywhere in the file. The characters defined between the quotation marks will replace the default comment characters mentioned previously. The new comment characters will be valid from the point the line is inserted to the end of the file, or another [Comment chars] line is inserted. The following example would replace * and ; with | (pipe) as the only valid comment character.

[Commant chars] "|"

Delimiter Characters
White space can be overridden using the following syntax:

[Delimiter chars] ",()"

This statement can appear anywhere in the file. The characters defined between the quotation marks will replace the default white space characters mentioned previously. The new white space characters will be valid from the point the line is inserted to the end of the file, or another [Delimiter chars] line is inserted. The following example would be valid using the default model settings:

(time,voltage) (time,voltage)
(time,voltage) (time,voltage)
(time,voltage) (time,voltage)

If you were to insert,

[Delimiter char] “”
You would not be able to use the time voltage pairings just shown.

Errors Checking
The model checks for an even number of point pairs (both x nd y values), invalid characters in a line, and non-increasing time. In each case where an error is found the filename and line number will be displayed in the IsSpice4 error file.

Port Table

Port_Name:	out
Description:	“output”
Direction:	out
Default_Type:	v
Allowed_Types:	[v,vd,i,id]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	no

Parameter Table

Parameter_Name:	input_file
Description:	“input filename”
Data_Type:	string
Default_Value:	“source.txt”
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	no

Parameter Table

Parameter_Name:	repeat
Description:	“repeat”
Data_Type:	boolean
Default_Value:	TRUE
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Sample PWL Files

```
* An example pwl file
[Comment chars]  “*|”
[Delimieter chars]  “,()”
* A really long test
+ 0.000000 0 0.000500 27 0.042000 27 0.042500 0 |more comments
+ (0.050000,0) (0.050500,27) (0.092000,27) (0.092500,0)
...
...



* Another example pwl file (some pairs with spaces, some with tabs)
 0.0 1.0
 1.0u   2.0
 2.0u   3.0
 3.0u   4.0
 4.0u 3.0
5.0u 0.0
```

Hybrid Code Models and Node Bridges

IsSpice4 is a mixed-mode simulator that contains both analog and event-driven simulators. This means that any simulation may contain components that are analog, event-driven, or a combination of both. During a mixed-mode simulation, the analog and the event-driven elements and simulation algorithms must communicate between each other. The simulator communication is handled by IsSpice4.

See Chapter 4 for information on node types.

Elements are classified as analog, event-driven (digital, real, user-defined), or hybrid (analog and event-driven) based on their node types. Each input or output is of a specific type. IsSpice4 models may have either analog or event-driven node types. An element that uses both analog and event-driven nodal connections is called a “hybrid”. Elements which use different node types must communicate through special elements called “Node Bridges”. The following hybrids and node bridges are supplied with IsSpice4.

Model Type	Device
Dac_bridge	Digital-to-Analog Node Bridge
Adc_bridge	Analog-to-Digital Node Bridge
D_to_real	Digital-to-Real Node Bridge
Real_to_v	Real-to-Analog Node Bridge
V_to_Real	Analog-to-Real Node Bridge
D_osc	Controlled Digital Oscillator
D_pwm	Controlled Digital Pulse Width Modulator

Digital-to-Analog Node Bridge

Format: A*name [Inputs N1.Nn-1] [Outputs Nn Nn+1.] modname*
.Model *modname* dac_bridge(pn1=*pv1....*)

Example: Abridge1 [7] [2] dac1
.Model dac1 dac_bridge(out_low = 0.7
+ out_high = 3.5 out_undef = 2.2
+ input_load = 5.0P t_rise = 50N f_fall = 20N)

The digital-to-analog bridge is the first of two node bridges which were designed to transfer digital, event-driven, information to analog values and back again. The second device is the analog-to-digital bridge. The input to a D-to-A bridge is a digital state from a digital node. This value, by definition, may only be 0, 1 or U. The D-to-A bridge then outputs the value “out_low”, “out_high” or “out_undef”, or ramps linearly toward one of these “final” values from its current analog output level. The speed at which this ramping occurs depends on the values of “t_rise” and “t_fall”. These parameters are interpreted by the model such that the rise or fall slope generated is always constant.

The dac_bridge determines the presence of the out_undef parameter. If this parameter is not specified, and if the out_high and out_low values are specified, then out_undef is assigned the value of the arithmetic mean of out_high and out_low. This simplifies coding of output buffers, where typically a logic family will include an out_low and out_high voltage, but not an out_undef value.

Since the D-to-A bridge accepts vector connections, multiple signals can be translated with a single bridge. For example, a two input two output D-to-A bridge could be written as:
“Abridge2 [a x] [b y] dac2”.

This model also posts an input load value (in farads) based on the parameter input_load. However, the output of this model does not respond to the total loading seen at its output.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	v
Allowed_Types:	[d]	[v,vd,i,id,d]
Vector:	yes	yes
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	out_low
Description:	“analog output for ‘ZERO’ digital input”
Data_type:	real
Default_Value:	0.0
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Parameter_Name:	out_high
Description:	“analog output for ‘ONE’ digital input”
Data_Type:	real
Default_Value:	1.0
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Parameter_Name:	out_undef	input_load
Description:	“analog output for ‘U’ input”	“input load (F)”
Data_Type:	real	real
Default_Value:	(out_high - out_low)/2	1.0e-12
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	t_rise	t_fall
Description:	“rise time”	“fall time”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	[1e-12 -]	[1e-12 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Analog-to-Digital Node Bridge

Format: A*name [Inputs N1.Nn-1] [Outputs Nn Nn+1.] modname*
.Model *modname* adc_bridge(pn1=*pv1...*)

Example: Abridge2 [1] [8] adc1
.Model adc_buff adc_bridge(in_low = 0.3
+ in_high = 3.5 rise_delay=10n)

The adc_bridge is one of two node bridges that have been designed to allow transfer of analog information to digital values and back again. The second device is the dac_bridge.

The input to an A-to-D bridge is an analog value from an analog node. This value, by definition, may be in the form of a voltage, or a current. If the input value is less than or equal to in_low, then a digital output value of “0” is generated. If the input is greater than or equal to in_high, a digital output value of “1” is generated. If neither of these is true, then a digital “UNKNOWN” state is generated. Note that unlike the case of the D-to-A bridge, no ramping time or delay is associated with the A-to-D bridge. Rather, the continuous ramping of the input value provides for any associated delays in the digitized signal.

Since the A-to-D bridge accepts vector connections, multiple signals can be translated with a single bridge. For example, a two-input two-output A-to-D bridge could be written as: “Abridge2 [a x] [b y] adc2”.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	v	d
Allowed_Types:	[v,vd,i,id,d,vnam]	[d]
Vector:	yes	yes
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	in_low	
Description:	“maximum 0-valued analog input”	
Data_Type:	real	
Default_Value:	0.1	
Limits:	-	
Vector:	no	
Vector_Bounds:	-	
Null_Allowed:	yes	
Parameter_Name:	in_high	
Description:	“minimum 1-valued analog input”	
Data_Type:	real	
Default_Value:	0.9	
Limits:	-	
Vector:	no	
Vector_Bounds:	-	
Null_Allowed:	yes	
Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Digital-to-Real Node Bridge

Format: A*name Input Enable Output modname*
.Model *modname* d_to_real(pn1=*pv1* pn2=*pv2*)

Example: Atest1 1 2 3 d_to_real
.Model adc1 d_to_real(zero = 0.1 one=.9
+ delay=5N)

The digital-to-real bridge translates digital states into real values. It accepts a digital value, 0, 1, or U, and creates a real-valued output from the zero or one model parameters after the specified delay. If the input is unknown, then the mean of the zero and one values is used as output. The second node is an enable that should be set to 0 (disable) or 1 (enable).

Port Table

Port_Name:	in	enable	out
Description:	“input”	“enable”	“output”
Direction:	in	in	out
Default_Type:	d	d	real
Allowed_Types:	[d]	[d]	[real]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	no	yes	no

Parameter Table

Parameter_Name:	zero	one	delay
Description:	“value for 0”	“value for 1”	“delay”
Data_Type:	real	real	real
Default_Value:	0.0	1.0	1e-9
Limits:	-	-	[1e-15 -]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Real-to-Analog Node Bridge

Format: A*name Input Output modname*
.Model *modname* real_to_v(pn1=*pv1...*)

Example: Atest1 1 2 rtv
.Model rtv real_to_v(gain = 1 transition_time=2N)

The real-to-analog bridge translates real values to analog voltages. It accepts a real value and creates an analog output that reflects the input, multiplied by the gain factor over the transition time.

Port Table

Port_Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	real	v
Allowed_Types:	[real]	[v, vd, i, id]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	gain	transition_time
Description:	“gain”	“output transition time”
Data_Type:	real	real
Default_Value:	1.0	1e-9
Limits:	-	[1e-15 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

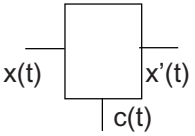
Analog-to-Real Node Bridge

Format: A*name Input Clock Output modname*
.Model modname a_to_r2(pn1=pv1...)

Example: Atest1 1 2 rtv
.Model rtv a_to_r2(gain = 1 transition_time=2N)

The analog to real bridge is designed to translate analog voltages to real values. It accepts an analog value and creates a real output that reflects the input multiplied by the gain factor.

This model is essentialy an Impulse Sampler of the form:



where x(t) is a continuous input signal and c(t) is a impulse modulator with

$c(t) = \Sigma\ \sigma(t-nT)$ from $-\infty$ to ∞

The output x'(t) is: $\Sigma\, x(nT)\ \sigma(t-nT)$ from $-\infty$ to ∞

where x(t) is an analog port, c(t) is a digital port, and x'(t) is a real port

The input, x(t) is sampled at every positive clock edge, c(t). This sample is multiplied by the gain parameter to create the output. The output of this device is delayed one clock period, T.

Port Table

Port_Name:	in	clk	out
Description:	“input”	“clock”	“output”
Direction:	in	in	out
Default_Type:	v	d	real2
Allowed_Types:	[v]	[d]	[real2]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	no	no	no

Parameter Table

Parameter_Name:	gain	clk_delay
Description:	“gain”	“delay at clk”
Data_Type:	real	real
Default_Value:	1.0	1e-9
Limits:	-	[1e-15 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Controlled Digital Oscillator

Format: A*name Control_Input Output modname*
.Model *modname* d_osc(pn1=*pv1* pn2=*pv2...*)

Example:
```
A5 1 8 var_clock
.Model var_clock d_osc(
+ cntl_freq_array = [-2,1K -1,1K 1,10K 2,10K]
+ duty_cycle = 0.4 init_phase = 180.0
+ rise_delay = 10N fall_delay=8N)
```

The digital oscillator is a hybrid model that accepts an analog voltage or current input. This input is compared with the voltage-to-frequency transfer characteristic specified by the cntl_freq_array coordinate pairs, and obtains a frequency that represents a linear interpolation of those pairs. A digital signal is then produced with this fundamental frequency.

The cntl_freq_array values represent coordinate points on the x and y axes, respectively, and normally represent voltage and frequency pairings. There may be as few as two pairs specified, or as many as memory and simulation speed allow. This permits you to very finely approximate a nonlinear function of frequency by entering multiple input-output coordinate points. Cntl_freq_arrays with 2 x, y points will yield a linear variation of frequency with respect to the control input. Greater array sizes will yield a piecewise linear response.

The output waveform has rise and fall delays, which can be specified independently. The duty cycle and the initial phase of the waveform may also be set.

Port Table

Port Name:	cntl_in	out
Description:	“control input”	“output”
Direction:	in	out
Default_Type:	v	d
Allowed_Types:	[v,vd,i,id]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	cntl_freq_array	
Description:	“control/freq array”	
Data_Type:	real	
Default_Value:	-	
Limits:	-	
Vector:	yes	
Vector_Bounds:	[2 -]	
Null_Allowed:	no	

Parameter_Name:	duty_cycle	init_phase
Description:	“duty cycle”	“initial phase of output”
Data_Type:	real	real
Default_Value:	0.5	0
Limits:	[1e-6 0.999999]	[-180.0 +360.0]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1e-9	1e-9
Limits:	[0 -]	[0 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Controlled Digital PWM

Format: A*name Input Output modname*
.Model *modname* d_pwm(pn1= *pv1* pn2= *pv2*...)

Example: A5 1 8 pwm
.Model pwm d_pwm (cntl_pw_array = [0 .1 1 .9]
+ frequency = 1meg rise_delay = 10N
+ fall_delay=8N)

The digital pulse width modulator (PWM) is a hybrid code model. It accepts an analog voltage or current input signal. This input is compared with the piece-wise linear voltage-to-pulse width transfer characteristic specified by the cntl_pw_array coordinate pairs, and obtains a pulse width which represents a linear interpolation of those pairs. A digital signal is then produced with this pulse width at the frequency specified by the frequency parameter.

The cntl_pw_array values represent coordinate points on the x and y axes, respectively, and normally represent voltage and frequency pairings. There may be as few as two pairs specified, or as many as memory and simulation speed allow. This permits you to very finely approximate a nonlinear function of control signal versus pulse width by entering multiple input-output coordinate points. Cntl_pw arrays with 2 x, y points will yield a linear variation of frequency with respect to the control input. Greater array sizes will yield a piece-wise linear response.

The output waveform has rise and fall delays which can be specified independently.

Port Table

Port Name:	cntl_in	out
Description:	“control input”	“output”
Direction:	in	out
Default_Type:	v	d
Allowed_Types:	[v,vd,i,id]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	cntl_freq_array
Description:	“control/freq array”
Data_Type:	real
Default_Value:	-
Limits:	-
Vector:	yes
Vector_Bounds:	[2 -]
Null_Allowed:	no

Parameter_Name:	duty_cycle
Description:	“duty cycle”
Data_Type:	real
Default_Value:	0.5
Limits:	[0.01 0.99]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1e-9	1e-9
Limits:	[0 -]	[0 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Real Code Models

Real models differ from analog models in that they only store continuous real values, not complex values, and are processed by the event-driven simulation algorithm. The following real models are provided with IsSpice4.

Model Type	Device
real_delay	Z-Transform
real_gain	Gain Block

Z-Transform Block (Real)

Format: A*name Input Clock Output modname*
.Model *modname* real_delay(pn1=*pv1*)

Example: Atest1 1 2 3 delay
.Model delay real_delay(delay = 1u)

This hybrid block performs a unit delay specified by the delay model parameter. The second node must be a digital signal, while the first and last must be connected to real node types.

Port Table

Port_Name:	in	clk	out
Description:	“input”	“clock”	“output”
Direction:	in	in	out
Default_Type:	real	d	real
Allowed_Types:	[real]	[d]	[real]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	no	no	no

Parameter Table

Parameter_Name:	delay
Description:	“delay from clk to out”
Data_Type:	real
Default_Value:	1e-9
Limits:	[1e-15 -]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Gain Block (Real)

Format: A*name Input Output modname*
.Model *modname* real_gain(pn1=*pv1*)

Example: Atest1 1 2 gain1
.Model gain1 real_gain(in_offset=.1 gain=1
+ delay=10N IC=1)

This element provides a simple gain function for a real-valued input. The output = gain ∗ (input + in_offset) + out_offset and is delayed by the delay model parameter.

Port Table

Port_Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	real	real
Allowed_Types:	[real]	[real]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	in_offset	gain	out_offset
Description:	“input offset”	“gain”	“output offset”
Data_Type:	real	real	real
Default_Value:	0.0	1.0	0.0
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	delay	ic
Description:	“delay”	“initial condition”
Data_Type:	real	real
Default_Value:	1.0e-9	0.0
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Digital Code Models

All digital code models are processed by the event-driven simulator in IsSpice4. All digital nodes are initialized to ZERO at the start of a simulation. All of the basic digital gates, flip-flops, and latches drive their outputs with a STRONG digital signal strength. In general, any unknown, or floating input will cause an output to be unknown. Most digital elements allow their rising and falling delays to be independently set.

The digital models post an input load value (in farads) which are based on the parameter input_load. The outputs of these models DO NOT, however, respond to the total loading it sees on their output. Unless undefined, they will always drive their outputs strongly with the delays specified by the delay-related model parameters.

Note: In order to communicate with analog, real, or other user-defined node types, node bridges must be used.

The following digital code models are included with IsSPICE4:

Model Type	Device
D_buffer	Buffer
D_Inverter	Inverter
D_And	And
D_Nand	Nand
D_Or	Or
D_Nor	Nor
D_Xor	Xor
D_Xnor	Xnor
D_Tristate	Tristate
D_Pullup	Pullup
D_Pulldown	Pulldown
D_Open_C	Open Collector
D_Open_E	Open Emitter

Model Type	Device
D_DFF	D Flip Flop
D_JKFF	JK Flip Flop
D_TFF	Toggle Flip Flop
D_SRFF	Set-Reset Flip Flop
D_Dlatch	D Latch
D_SRlatch	Set-Reset Latch
D_State	State Machine
D_FDIV	Frequency Divider
D_Ram	RAM
D_Source	Digital Source
NCO	MIDI Digitally controlled oscillator

Buffer

Format: A*name Input Output modname*
.Model *modname* d_buffer(pn1=*pv1...*)

Example: A1 1 8 buff1
.Model buff1 d_buffer(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The buffer is a single-input, single-output buffer that produces a time-delayed copy of its input.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Inverter

Format: A*name Input Output modname*
.Model *modname* d_inverter(pn1=*pv1*...)

Example: A1 1 8 inv1
.Model inv1 d_inverter(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The inverter is a single-input, single-output inverter that produces an inverted, time-delayed copy of its input.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

And

Format: A*name [Input Bus Nodes: N1 N2..Nn]*
+ Output: Nn+1 modname
.Model *modname* d_and(pn1=*pv1...*)

Example: A6 [1 2] 8 and1
.Model and1 d_and(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The and gate is an n-input, single-output gate that produces an active 1 value if, and only if, all of its inputs are also 1 values. If one or more of the inputs is a 0, the output will also be a 0. If neither of these conditions exists, the output will be unknown. Note that since the input port type is a vector, any number of inputs may be specified.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Nand

Format: A*name [Input Bus Nodes: N1 N2..Nn]*
+ Output: Nn+1 modname
.Model *modname* d_nand(pn1=*pv1*...)

Example: A1 [1 2 3] 8 nand1
.Model nand1 d_nand(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The nand gate is an n-input, single-output gate that produces an active 0 value if and only if all of its inputs are 1. If one or more of the inputs is a 1, the output will be a 0. If neither of these conditions exists, the output will be unknown. Since the input port type is a vector, any number of inputs may be specified.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Or

Format: A*name [Input Bus Nodes: N1 N2..Nn]*
+ Output: Nn+1 modname
.Model *modname* d_or(pn1=*pv1...*)

Example: A1 [1 2 3] 8 or1
.Model or1 d_or(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The or gate is an n-input, single-output gate that produces an active 1 if at least one of its inputs is a 1. The gate produces a 0 value if all inputs are 0. If neither of these two conditions exists, the output is unknown. Note that since the input port type is a vector, any number of inputs may be specified.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Nor

Format: A*name [Input Bus Nodes: N1 N2..Nn]*
+ Output: Nn+1 modname
.Model *modname* d_nor(pn1=*pv1...*)

Example: Anor12 [1 2 3 4] 8 nor12
.Model nor12 d_or(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The nor gate is an n-input, single-output gate that produces an active 0 value if at least one of its inputs is a 1 value. The gate produces a 1 value if all inputs are 0; if neither of these two conditions exists, the output is unknown. Since the input port type is a vector, any number of inputs may be specified.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Xor

Format: A*name [Input Bus Nodes: N1 N2..Nn]*
+ Output: Nn+1 modname
.Model *modname* d_xor(pn1=*pv1...*)

Example: A9 [1 2] 8 xor3
.Model xor3 d_xor(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The xor gate is an n-input, single-output gate that produces an active 1 value if an odd number of its inputs are 1 values. Note that since the input port type is a vector, any number of inputs may be specified.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Xnor

Format: A*name [Input Bus Nodes: N1 N2..Nn]*
+ Output: Nn+1 modname
.Model *modname* d_xnor(pn1=*pv1...*)

Example: a9 [1 2] 8 xnor3
.Model xnor3 d_xnor(rise_delay = 0.5N
+ fall_delay = 0.3N input_load = 0.5P)

The xnor gate is an n-input, single-output gate that produces an active 0 value if an odd number of its inputs are 1 values. It produces a 1 output when an even number of 1 values occurs on its inputs. Note that since the input port type is a vector, any number of inputs may be specified.

Port Table

Port Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[2 -]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	fall_delay	input_load
Description:	“rise delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Tristate

Any UNKNOWN or floating input causes the output to become UNKNOWN.

Any UNKNOWN input on the enable line causes the output to become an UNDETERMINED strength.

Format: A*name Input Enable Output modname*
.Model *modname* d_tristate(pn1=*pv1...*)

Example: A1 1 2 8 tri7
.Model tri7](delay = 0.5N
+ input_load = 0.5P enable_load = 0.5P)

The tristate is a simple tristate gate that can be configured to allow for open-collector behavior, as well as standard tristate behavior. The state of the input line is reflected in the output. The state seen on the enable line determines the strength of the output. Thus, a ONE forces the output to its state with a STRONG strength. A ZERO forces the output to go to a HI_IMPEDANCE strength. The delays associated with an output state or strength change cannot be specified independently, nor can they be specified independently for rise or fall conditions. Other gate models may be used to provide such delays, if needed.

Port Table

Port Name:	in	enable	out
Description:	“input”	“enable”	“output”
Direction:	in	in	out
Default_Type:	d	d	d
Allowed_Types:	[d]	[d]	[d]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	no	no	no

Parameter Table

Parameter_Name:	delay	input_load	enable_load
Description:	“delay”	“input load value (F)”	“enable load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-12	1.0e-12
Limits:	[1.0e-12 -]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Pullup

Format: A*name Output modname*
.Model *modname* d_pullup(pn1=*pv1*)

Example: A2 9 pullup1
.Model pullup1 d_pullup(load = 20P)

The pullup resistor is a device that emulates the behavior of an analog resistance value that is tied to a high voltage level. The pullup may be used in conjunction with tristate buffers to provide open-collector wired "or" constructs, or any other logical constructs that rely on a resistive pullup, which is common to many tristated output devices.

Note: The output of this device is a logical 1. Hence, this device may be connected to any digital node that requires a constant high state.

Port Table

Port Name:	out
Description:	"output"
Direction:	out
Default_Type:	d
Allowed_Types:	[d]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	no

Parameter Table

Parameter_Name:	load
Description:	"load value (F)"
Data_Type:	real
Default_Value:	1.0e-12
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Pulldown

Format: A*name Output modname*
.Model *modname* d_pulldown(pn1=*pv1*)

Example: A4 9 pulldown1
.Model pulldown1 d_pulldown(load = 20P)

The pulldown resistor is a device which emulates the behavior of an analog resistance value which is tied to a low voltage level. The pulldown may be used in conjunction with tristate buffers to provide open-collector wired "or" constructs, or any other logical constructs which rely on a resistive pulldown which is common to many tristated output devices.

The output of this device is a logical 0. Hence, this device may be connected to any digital node that requires a constant low state.

Port Table

Port Name:	out
Description:	"output"
Direction:	out
Default_Type:	d
Allowed_Types:	[d]
Vector:	no
Vector_Bounds:	-
Null_Allowed:	no

Parameter Table

Parameter_Name:	load
Description:	"load value (F)"
Data_Type:	real
Default_Value:	1.0e-12
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Open Collector

Format: A*name Input Output modname*
.Model *modname* d_open_c(pn1=*pv1*...)

Example: A4 9 10 openc
.Model openc d_open_c(open_delay=5n fall_delay=10n)

If the input to this device is a 1 then the output is a 1, with a HI_IMPEDANCE strength. If the input is a 0, then the output is a STRONG 0, otherwise, the output strength is UNDETERMINED. The falling (fall_delay) and rising (open_delay) delays may be specified independently.

Port Table

Port_Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	open_delay	fall_delay	input_load
Description:	“open delay”	“fall delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1e-12 -]	[1e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Open Emitter

Format: A*name Input Output modname*
.Model *modname* d_open_e(pn1=*pv1* pn2=*pv2..*)

Example: a4 9 10 opene
.Model opene d_open_e(rise_delay=10n...)

If the input to this device is a 1, then the output is a 1 with a STRONG. If the input is a 0, then the output is a HI_IMPEDANCE 0, otherwise, the output strength is UNDETERMINED. The falling (open_delay) and rising (rise_delay) delays may be specified independently.

Port Table

Port_Name:	in	out
Description:	“input”	“output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	rise_delay	open_delay	input_load
Description:	“rise delay”	“open delay”	“input load value (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-12
Limits:	[1e-12 -]	[1e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

D Flip Flop

Format: A*name Data_Input Clock Nset Nreset Data_Out*
+ Inverted_Data_Out modname
.Model *modname* d_dff(pn1=*pv1*...)

Example: A7 1 2 3 4 5 6 dflop1
.Model flop1 d_dff(clk_delay = 13.0n
+ nset_delay = 25.0n nreset_delay = 27.0n
+ ic = 2 rise_delay = 10.0n fall_delay = 3n)

The d-type flip flop is a one-bit, edge-triggered storage element which stores data whenever the clk input line transitions from 0 to 1. In addition, asynchronous set and reset signals exist, and each of the three methods of changing the stored output of the d-flip flop have separate load values and delays associated with them. Additionally, you may specify separate rise and fall delays that are added to those specified for the input lines. These allow for more faithful reproduction of the output characteristics of different IC fabrication technologies.

Any UNKNOWN input on the set or reset lines immediately results in an UNKNOWN output.

Port Table

Port Name:	data	clk	nset	nreset
Description:	“input data”	“clock”	“asynch. ~set”	“asynch. ~reset”
Direction:	in	in	in	in
Default_Type:	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	no	no	yes	yes

Port Name:	out	Nout
Description:	“data output”	“inverted data output”
Direction:	out	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter Table

Parameter_Name:	clk_delay	nset_delay	nreset_delay
Description:	“delay from clk”	“delay from set”	“delay from reset”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	ic	data_load	clk_load
Description:	“output initial state”	“data load (F)”	“clk load (F)”
Data_Type:	int	real	real
Default_Value:	0	1.0e-12	1.0e-12
Limits:	[0 2]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	nset_load	nreset_load
Description:	“set load value (F)”	“reset load (F)”
Data_Type:	real	real
Default_Value:	1.0e-12	1.0e-12
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

JK Flip Flop

Format: A*name J_Input K_Input Clock Set Reset*
+ Data_Out Inverted_Data_Out modname
.Model *modname* d_jkff(pn1=*pv1...*)

Example: A8 1 2 3 4 5 6 7 jkflop2
.Model flop2 d_jkff(clk_delay = 13.0n
+ set_delay = 25.0n reset_delay = 27.0n
+ ic = 2 rise_delay = 10.0n fall_delay = 3n)

The jk-type flip flop is a one-bit, edge-triggered storage element which will store data whenever the clk input line transitions from low to high. In addition, asynchronous set and reset signals exist, and each of the three methods of changing the stored output of the jk-flip flop have separate load values and delays associated with them. Additionally, you may specify separate rise and fall delays that are added to those specified for the input lines. This allows for a more faithful reproduction of the output characteristics of different IC fabrication technologies.

Any UNKNOWN inputs, other than j or k, cause the output to become UNKNOWN automatically.

Port Table

Port Name:	j	k	clk	set	reset
Description:	“j input”	“k input”	“clock”	“asynch. set”	“asynch. reset”
Direction:	in	in	in	in	in
Default_Type:	d	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]	[d]
Vector:	no	no	no	no	no
Vector_Bounds:	-	-	-	-	-
Null_Allowed:	no	no	no	yes	yes

Port Name:	out	Nout
Description:	“data output”	“inverted data output”
Direction:	out	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds	-	-
Null_Allowed:	yes	yes

Parameter Table

Parameter_Name:	clk_delay	set_delay	reset_delay
Description:	“delay from clk”	“delay from set”	“delay from reset”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	ic	jk_load	clk_load
Description:	“output initial state”	“j,k load (F)”	“clk load (F)”
Data_Type:	int	real	real
Default_Value:	0	1.0e-12	1.0e-12
Limits:	[0 2]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	set_load	reset_load
Description:	“set load value (F)”	“reset load (F)”
Data_Type:	real	real
Default_Value:	1.0e-12	1.0e-12
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Toggle Flip Flop

Format: A*name T_Input Clock Set Reset Data_Out*
+ Inverted_Data_Out modname
.Model *modname* d_tff(pn1=*pv1...*)

Example: A8 2 12 4 5 6 3 tflop3
.Model flop3 d_tff(clk_delay = 13.0n ic = 2
+ set_delay = 25.0n reset_delay = 27.0n
+ rise_delay = 10n fall_delay = 3n t_load = 0.2p)

Any UNKNOWN inputs other than t immediately cause the output to become UNKNOWN.

The toggle-type flip flop is a one-bit, edge-triggered storage element that will toggle its current state whenever the clk input line transitions from 0 to 1. In addition, asynchronous set and reset signals exist, and each of the three methods of changing the stored output of the t-flip flop have separate load values and delays associated with them. Additionally, you may specify separate rise and fall delay values that are added to those specified for the input lines. This allows for a more faithful reproduction of the output characteristics of different IC fabrication technologies.

Port Table

Port Name:	t	clk	set	reset
Description:	“toggle input”	“clock”	“asynch. set”	“asynch. reset”
Direction:	in	in	in	in
Default_Type:	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	no	no	yes	yes

Port Name:	out	Nout
Description:	“data output”	“inverted data output”
Direction:	out	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter Table

Parameter_Name:	clk_delay	set_delay	reset_delay
Description:	“delay from clk”	“delay from set”	“delay from reset”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no
Vector_Bounds	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	ic	t_load	clk_load
Description:	“output initial state”	“toggle load (F)”	“clk load (F)”
Data_Type:	int	real	real
Default_Value:	0	1.0e-12	1.0e-12
Limits:	[0 2]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	set_load	reset_load
Description:	“set load value (F)”	“reset load (F)”
Data_Type:	real	real
Default_Value:	1.0e-12	1.0e-12
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Set-Reset Flip Flop

Format: A*name S_Input R_Input Clock Set Reset*
+ Data_Out Inverted_Data_Out modname
.Model *modname* d_srff(pn1=*pv1...*)

Example: A8 2 12 4 5 6 3 14 srflop7
.Model flop7 d_srff(clk_delay = 13.0n
+ set_delay = 25.0n reset_delay = 27.0n
+ ic = 2 rise_delay = 10.0n fall_delay = 3n)

The set-reset type flip flop is a one-bit, edge-triggered storage element that will store data whenever the clk input line transitions from 0 to 1. The stored value (i.e., the "out" value) will depend on the s and r inputs, and will be:

out=ONE	if s=ONE and r=ZERO;
out=ZERO	if s=ZERO and r=ONE;
out=previous value	if s=ZERO and r=ZERO;
out=UNKNOWN	if s=ONE and r=ONE;

In addition, asynchronous set and reset signals exist, and each of the three methods of changing the stored output of the set-reset flip flop has separate load values and delays associated with them. You may also specify separate rise and fall delay values that are added to those specified for the input lines. This allows for a more faithful reproduction of the output characteristics of different IC fabrication technologies.

Any UNKNOWN inputs, other than s and r, immediately cause the output to become UNKNOWN.

Port Table

Port Name:	s	r	clk	set	reset
Description:	"set"	"reset"	"clock"	"asynch. set"	"asynch. reset"
Direction:	in	in	in	in	in
Default_Type:	d	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]	[d]
Vector:	no	no	no	no	no
Vector_Bounds:	-	-	-	-	-
Null_Allowed:	no	no	no	yes	yes

Port Name:	out	Nout
Description:	“data output”	“inverted data output”
Direction:	out	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter Table

Parameter_Name:	clk_delay	set_delay	reset_delay
Description:	“clk delay”	“set delay”	“reset delay”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	ic	sr_load	clk_load
Description:	“output initial state”	“s r load (F)”	“clk load (F)”
Data_Type:	int	real	real
Default_Value:	0	1.0e-12	1.0e-12
Limits:	[0 2]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	set_load	reset_load	rise_delay	fall_delay
Description:	“a.set load (F)”	“a.reset load (F)”	“rise delay”	“fall delay”
Data_Type:	real	real	real	real
Default_Value:	1.0e-12	1.0e-12	1.0e-9	1.0e-9
Limits:	-	-	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

D Latch

Format: A*name Data_Input Enable Set Reset Data_Out*
+ Inverted_Data_Out modname
.Model *modname* d_dlatch(pn1=*pv1...*)

Example:
```
A4 12 4 5 6 3 14 dlatch1
.Model latch1 d_dlatch(data_delay = 13n
+ enable_delay = 22n set_delay = 25n
+ reset_delay = 27n ic = 2 rise_delay = 10n
+ fall_delay = 3n)
```

The d-type latch is a one-bit, level-sensitive storage element that will output the value on the data line when the enable input line is high. The value on the data line is held on the out line when the enable line is low.

In addition, asynchronous set and reset signals exist, and each of the four methods of changing the stored output of the D latch (i.e., data changing with enable=ONE, enable changing to ONE from ZERO with a new value on data, raising set and raising reset) has separate delays associated with them. You may also specify separate rise and fall delays that are added to those specified for the input lines. This allows for a more faithful reproduction of the output characteristics of different IC fabrication technologies.

Any UNKNOWN inputs, other than on the data line when enable=ZERO, cause the output to become UNKNOWN.

Port Table

Port Name:	data	enable	set	reset
Description:	“data in”	“enable in”	“set”	“reset”
Direction:	in	in	in	in
Default_Type:	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	no	no	yes	yes

Port Name:	out	Nout
Description:	“data output”	“inverter data output”
Direction:	out	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter Table

Parameter_Name:	data_delay	enable_delay	set_delay	reset_delay
Description:	“data delay”	“enable delay”	“s delay”	“r delay”
Data_Type:	real	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

Parameter_Name:	ic	data_load	enable_load
Description:	“output initial state”	“data load (F)”	“enable load (F)”
Data_Type:	int	real	real
Default_Value:	0	1.0e-12	1.0e-12
Limits:	[0 2]	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	set_load	reset_load	rise_delay	fall_delay
Description:	“set load (F)”	“reset load (F)”	“rise delay”	“fall delay”
Data_Type:	real	real	real	real
Default_Value:	1.0e-12	1.0e-12	1.0e-9	1.0e-9
Limits:	-	-	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no	no
Vector_Bounds:	-	-	-	-
Null_Allowed:	yes	yes	yes	yes

Set-Reset Latch

Format: A*name S_In R_In Enable Set Reset Data_Out*
+ Inverted_Data_Out modname
.Model *modname* d_srlatch(pn1=*pv1...*)

Example:
```
A4 12 4 5 6 3 14 16 srlatch2
.Model latch2 d_srlatch(sr_delay = 13n
+ enable_delay = 22n set_delay = 25n
+ reset_delay = 27n ic = 2 rise_delay = 10n)
```

The set-reset type latch is a one-bit, level-sensitive storage element that will output the value dictated by the state of the s and r pins whenever the enable input line is high. This value is held at the output whenever the enable line is low. The particular value chosen is as shown below:

s=ZERO, r=ZERO	out=no change in output
s=ZERO, r=ONE	out=ZERO
s=ONE, r=ZERO	out=ONE
s=ONE, r=ONE	out=UNKNOWN

Asynchronous set and reset signals exist, and each of the four methods of changing the stored output of the set-reset latch (i.e., s/r combination changing with enable=ONE, enable changing to ONE from ZERO with an output-changing combination of s and r, raising set and raising reset) have separate delays associated with them. You may also specify separate rise and fall delays, which are added to those specified for the input lines. This allows for a more faithful reproduction of the output characteristics of different IC fabrication technologies.

Port Table

Port Name:	s	r	enable	set	reset
Description:	“set”	“reset”	“enable”	“asynch set”	“asynch reset”
Direction:	in	in	in	in	in
Default_Type:	d	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]	[d]
Vector:	no	no	no	no	no
Vector_Bounds:	-	-	-	-	-
Null_Allowed:	no	no	no	yes	yes

Port Name:	out	Nout
Description:	“data output”	“inverted data output”
Direction:	out	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	sr_delay	enable_delay	set_delay
Description:	“s/r delay”	“enable delay”	“asynch s delay”
Data_Type:	real	real	real
Default_Value:	1.0e-9	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	reset_delay	ic
Description:	“asynch r delay”	“output initial state”
Data_Type:	real	int
Default_Value:	1.0e-9	0
Limits:	[1.0e-12 -]	[0 2]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	sr_load	enable_load	set_load
Description:	“s/r input loads (F)”	“enable load (F)”	“set load (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-12	1.0e-12	1.0e-12
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	reset_load	rise_delay	fall_delay
Description:	“reset load (F)”	“rise delay”	“fall delay”
Data_Type:	real	real	real
Default_Value:	1.0e-12	1.0e-9	1.0e-9
Limits:	-	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

State Machine

Format: A*name [Input Bus Nodes: N1... Nn-2] Clock*
+ Reset [Out Bus Nodes: Nn+1... Nm]
+ modname
.Model *modname* d_state(pn1=*pv1*...)

Example: A4 [2 3 4 5] 1 12 [22 23 24 25 26 27 28 29] state1
.Model state1 d_state(clk_delay = 13N
+ reset_delay = 27N state_file = newstate.txt
+ reset_state = 2)

The state machine provides for straight forward descriptions of clocked combinational logic blocks with a variable number of inputs and outputs and an unlimited number of states. The model can be configured to behave as virtually any type of counter or clocked combinational logic block and can be used to replace very large sections of digital circuits with an identically functional but faster representation.

The inputs consist of a vector set of inputs, a single clock, a single reset line, and a vector set of outputs. The clk_delay parameter specifies the time after the POSITIVE clk signal edge that the outputs will transition. The reset_delay parameter specifies the time after the POSITIVE reset signal edge that the outputs will transition to the state number defined by the reset_state parameter.

The state machine is configured through the use of a separate ASCII state definition text file. This file should be located in your current working directory. It can be created and edited with any text editor such as Word, DOS Edit, or ISEd. The filename is arbitrary but must match the state_file model parameter string. You may add a path to the file, i.e. “C:\MyFiles\newstate.txt”.

The search path for the state transition file takes the following route; first IsSpice4 looks in the explicit path, if one is stated, then it looks in you current working directory, then it looks in the directory designated by the ISLIB environment variable, if one

is entered, and lastly IsSpice4 looks in the IsSpice4 executable directory (SPICE8\IS).

The file defines all states to be understood by the model, plus input bit combinations which trigger changes in state. An example state file is shown next.

This is an example state input file that defines a simple 2-bit counter (2 outputs) with one input signal. The value of this input determines whether the counter counts up (in = 1) or down (in = 0). When used with the example on the previous page, this file would be saved as “newstate.txt”.

```
* This is an example state input file
* that define a 2-bit up/down counter.
*The entries have been spaced for easy reading
*Present    Outputs          Input(s)    Destination
*State      @this State
0           0s      0s       0           3
                             1           1

1           0s      1z       0           0
                             1           2

2           1z      0s       0           1
                             1           3

3           1z      1z       0           2
                             1           0
```

Strengths
s=strong
u=undetermined
r=resistive
z=hi_impedance

Input(s) are those input signals that when clocked by a positive edge on the clk input, will give the states listed in the **Destination** column. For example, if the machine is in the 1 state and the input is a 1, then at the next positive clk edge, the outputs will be set to 1z and 0s (state 2).

Several attributes of the above file structure should be noted. First, ALL LINES IN THE FILE MUST BE ONE OF FOUR TYPES. These are:

A header line, which is a complete description of the current state, the outputs corresponding to that state, an input value, and the state that the model will assume if that input is encountered. The first line of a state definition must ALWAYS be a header line.

A continuation line, which is a partial description of a state, consisting of an input value and the state that the model will assume if that input is encountered. Note that continuation lines may only be used after the initial header line definition for a state.

A line containing nothing but white space (space, formfeed, newline, carriage return, tab, vertical tab).

A comment, beginning with a "*" in the first column.

A line that is not one of the above will cause a file-loading error. In the example shown, white space (any combination of blanks, tabs, commas) is used to separate values, and the characters "->" are used to underline the state transition that is implied by the input that precedes it. This particular character is not critical, and may be replaced with any other character or non-broken combination of characters (e.g. "==>", ">>", ":", etc.)

The order of the output and input bits in the file is important; the first column is always interpreted as the "zeroth" bit of input and output. Thus, in the file above, the output from state 1 sets out[0] to "0s", and out[1] to "1z".

The state numbers don't need to be in any particular order, but a state definition that consists of the sum total of all lines, which define the state, its outputs, and all methods by which a state can be exited, must be made on contiguous line numbers. A single state definition cannot be broken into sub-blocks and distributed randomly throughout the file. On the other hand, the state definition may be broken up by as many comment lines as you desire.

Port Table

Port Name:	in	clk	reset	out
Description:	“input”	“clock”	“reset”	“output”
Direction:	in	in	in	out
Default_Type:	d	d	d	d
Allowed_Types:	[d]	[d]	[d]	[d]
Vector:	yes	no	no	yes
Vector_Bounds:	[1 -]	-	-	[1 -]
Null_Allowed:	yes	no	yes	no

Parameter Table

Parameter_Name:	clk_delay	reset_delay	state_file
Description:	“CLK delay”	“RESET delay”	“state definition file name”
Data_Type:	real	real	string
Default_Value:	1.0e-9	1.0e-9	“state.txt”
Limits:	[1.0e-12 -]	[1.0e-12 -]	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	no

Parameter_Name:	input_load	clk_load	reset_load
Description:	“input load (F)”	“clock load (F)”	“reset load (F)”
Data_Type:	real	real	real
Default_Value:	1.0e-12	1.0e-12	1.0e-12
Limits:	-	-	-
Vector:	no	no	no
Vector_Bounds:	-	-	-
Null_Allowed:	yes	yes	yes

Parameter_Name:	reset_state
Description:	“default state on RESET & at DC”
Data_Type:	int
Default_Value:	0
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	no

Frequency Divider

Format: A*name Freq_Input Freq_Output modname*
.Model *modname* d_fdiv(pn1=*pv1...*)

Example: A4 3 7 divider
.Model divider d_fdiv(div_factor=5 high_cycles=3
+ i_count = 4 rise_delay = 23n fall_delay = 9n)

The frequency divider is a programmable step-down divider, which accepts an arbitrary divisor (div_factor), a duty-cycle term (high_cycles), and an initial count value (i_count). The generated output is synchronized to the rising edges of the input signal. The rise and fall delay of the output may also be specified independently.

Port Table

Port Name:	freq_in	freq_out
Description:	“freq. input”	“freq. output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	div_factor	high_cycles
Description:	“divide factor”	“# of cycles for high out”
Data_Type:	int	int
Default_Value:	2	1
Limits:	[1 -]	[1 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	i_count	freq_in_load
Description:	“divider initial count value”	“freq_in load (F)”
Data_Type:	int	real
Default_Value:	0	1.0e-12
Limits:	[0 -]	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	rise_delay	fall_delay
Description:	“rise delay”	“fall delay”
Data_Type:	real	real
Default_Value:	1.0e-9	1.0e-9
Limits:	[1.0e-12 -]	[1.0e-12 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

RAM

Format:
A*name [Data_In Nodes: N1... Nn-2]*
+ [Data_Out Nodes: Nn-1... Nn]
+ [Address Nodes: Nn+1... Nm-1]
+ Write_Enable [Select Nodes: Nm+1... Nz]
+ modname
.Model *modname* d_ram(pn1=*pv1*...)

Example:
A4 [3 4 5 6] [3 4 5 6] [12 13 14 15 16 17 18 19] 30
+ [22 23 24] ram2
.Model ram2 d_ram(select_value = 2 ic = 1
+ read_delay = 80n)

RAM is an M-wide, N-deep random access memory element with programmable select lines, tristated data out lines, and a single write/read line. The width of the RAM words (M) is set by the number of inputs detected by the d_ram code model. The depth of the RAM (N) is set by the number of address lines that are input to the device. The value of N is related to the number of address input lines (P) by the following equation:

$$2^P = N$$

There is no reset line for the device. However, an initial value for all bits may be specified by setting the IC parameter to either 0 or 1. When reading, a word from the ram output will not appear until read_delay is satisfied. Separate rise and fall delays are not supported for this device.

UNKNOWN inputs on the address lines are not allowed during a write. In the event that an address line does indeed go unknown during a write, THE ENTIRE CONTENTS OF THE RAM WILL BECOME UNKNOWN. This is in contrast to the data_in lines that become unknown during a write; in that case, only the selected word will be corrupted, and it will be corrected once the data lines settle back to a known value. Protection is

added to the write_en line such that extended UNKNOWN values on that line are interpreted as ZERO values. This is the equivalent of a read operation and will not corrupt the contents of the RAM. A similar mechanism exists for the select lines. If they are unknown, then it is assumed that the chip is not selected.

Detailed timing-checking routines are not provided in this model, other than for the enable_delay and select_delay restrictions on read operations. You are advised, therefore, to carefully check the timing into and out of the RAM for correct read and write cycle times, setup and hold times, etc. for the particular device you are attempting to model.

Port Table

Port Name:	data_in	data_out
Description:	“data input line(s)”	“data output line(s)”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	yes
Vector_Bounds:	[1 -]	[1 -]
Null_Allowed:	no	no

Port Name:	address	write_en	select
Description:	“address input line(s)”	“write enable line”	“chip select line(s)”
Direction:	in	in	in
Default_Type:	d	d	d
Allowed_Types:	[d]	[d]	[d]
Vector:	yes	no	yes
Vector_Bounds:	[1 -]	-	[1 16]
Null_Allowed:	no	no	no

Parameter Table

Parameter_Name:	select_value	ic
Description:	“decimal active value for select line comparison”	“initial bit state @ dc”
Data_Type:	int	int
Default_Value:	1	2
Limits:	[0 32767]	[0 2]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter Table

Parameter_Name:	read_delay	select_load
Description:	“read delay from address/select/write_en active”	“select load value (F)”
Data_Type:	real	real
Default_Value:	100.0e-9	1.0e-12
Limits:	[1.0e-12 -]	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	data_load	address_load
Description:	“data_in load (F)”	“addr. load (F)”
Data_Type:	real	real
Default_Value:	1.0e-12	1.0e-12
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Parameter_Name:	enable_load
Description:	“enable line load value (F)”
Data_Type:	real
Default_Value:	1.0e-12
Limits:	-
Vector:	no
Vector_Bounds:	-
Null_Allowed:	yes

Digital Source

Format: A*name [N1...Nn] modname*
.Model *modname* d_source(pn1=*pv1...*)

Example: A1 [1 2 3 4 5 6 7 8] input
.Model input d_source(input_file = source.txt)

The digital source provides for straightforward descriptions of digital signal vectors in a tabular format. The model reads input from an ASCII text file and, at the times specified in the file, generates the inputs along with the strengths listed. This file should be located in your current working directory. It can be created and edited with any text editor such as Word, DOS Edit, or IsEd. The filename is arbitrary, but must match the input_file model parameter string. The format of the input file is as shown below. Comment lines are delineated via a single "*" character in the first column of a line.

Strengths
s=strong
u=undetermined
r=resistive
z=hi_impedance

```
*This is an example state input file
* T        c     n     n     n     . . .
* i        l     o     o     o     . . .
* m        o     d     d     d     . . .
* e        c     e     e     e     . . .
*          k     a     b     c     . . .

0.0000     Uu    Uu    Us    Uu    . . .
1.234e-9   0s    1s    1s    0z    . . .
1.376e-9   0s    0s    1s    0z    . . .
2.5e-7     1s    0s    1s    0z    . . .
2.506e-7   1s    1s    1s    0z    . . .
5.0e-7     0s    1s    1s    0z    . . .
```

Note that in the example shown, white space (any combination of blanks, tabs, commas) is used to separate the time and strength/state tokens. The order of the input columns is important. The first column is always interpreted as "time". The remaining columns are the desired outputs, and must match the order of the output nodes on the call line.

A non-commented line, which does not contain enough tokens to completely define all outputs for the digital source, will cause an error. Also, time values must increase monotonically or an error will result in reading the source file. Errors will also occur if a line in the source file is neither a comment nor a vector line. The only exception to this is in the case of a line that is completely blank.

Port Table

Port Name:	out
Description:	“output”
Direction:	out
Default_Type:	d
Allowed_Types:	[d]
Vector:	yes
Vector_Bounds:	-
Null_Allowed:	no

Parameter Table

Parameter_Name:	input_file	input_load
Description:	“input filename”	“input load (F)”
Data_Type:	string	real
Default_Value:	“source.txt”	1.0e-12
Limits:	-	-
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	no	no

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Format: A*name [Input Control Nodes: N1 N7] Output N8 + modname*
.Model *modname* nco(pn1=*pv1...*)

Example: Atest1 1 2 nco1
.Model nco1 nco(delay=1.0N Mult_Factor=16)

The MIDI VCO (NCO model) is an oscillator that produces a square wave whose frequency is based on a digital input. Both the input and output ports are vectors, but the input must consist of seven bits (MIDI note). MIDI notes are numbered between zero and 127 (Bit 1 is the MSB). Note: number zero corresponds to a C 5 octaves below middle C. There are 12 notes per octave, so a middle C (that is 261.62 Hz) is note number 60. A440 (A above middle C) is note number 69, and so forth. Square waves of different frequencies can be produced by changing the bit pattern and the mult_factor.

Port Table

Port_Name:	in	out
Description:	“program input”	“oscillator output”
Direction:	in	out
Default_Type:	d	d
Allowed_Types:	[d]	[d]
Vector:	yes	no
Vector_Bounds:	[7 7]	-
Null_Allowed:	no	no

Parameter Table

Parameter_Name:	delay	mult_factor
Description:	“output delay”	“freq multiplier”
Data_Type:	real	real
Default_Value:	1e-9	1
Limits:	[1e-15 -]	[1e-9 -]
Vector:	no	no
Vector_Bounds:	-	-
Null_Allowed:	yes	yes

Analysis Syntax

Analysis Notation

This chapter contains a complete list of the commands that control IsSpice4. The syntax used here follows the same format as that of the previous chapter.

Format: .PRINT type var1 [var2 ... varn]
.AC [DEC] [OCT] [LIN] np fstart fstop

Examples: .PRINT TRAN V(1)
.AC DEC 10 10 10MEG

The dot, "." preceding the command is required for all commands. Any exceptions are clearly stated. Items in italics must be replaced by user-defined data.

- For example, for the .PRINT statement, type, var1, var2, and so on, would be replaced with user-defined data.

The following description and examples will further clarify the required data.

.DC - DC Sweep Analysis

Format: .DC src start stop del [src2 start2 stop2 del2]

Examples: .DC VIN 0.25 5.0 0.25
.DC VDS 0 10 .5 VGS 0 5 1
.DC VCE 0 10 .25 IB 0 10U 1U

Summary: The .DC statement is a special subset of IsSpice4's DC analysis features. It is used to perform a series of DC operating points by sweeping voltage and/or current sources and performing a DC operating point at each step value of the source(s). At each step, voltages, currents, and a variety of device/model parameters can be recorded.

Syntax: The .DC line defines the source that is to be swept, and the sweep limits. Src is the name of the independent voltage or current source that will be swept. Start, stop, and del are the first, last, and incremental values, respectively. The first example will cause the value of the voltage source VIN to be swept from 0.25 Volts to 5.0 Volts in increments of 0.25 Volts. A second source (src2) may optionally be specified with associated sweep parameters (second example). In this case, the first source, VDS, will be swept over its range for each value of the second source, VGS.

The .DC statement overrides any DC voltage that is specified in the actual voltage/current source statement. The DC voltage on the V or I line will be used during the AC analysis and unless there is a transient specification, during the transient analysis. But when the DC sweep is run, the values that are specified in the .DC statement will prevail.

Getting Output: To generate output, the .DC statement must be accompanied by a .PRINT or .VIEW statement. Acceptable output variables are voltages, currents and computed device/model parameters. For example, .PRINT DC V(4) @R1[i], which was used with the first example .DC statement above, will yield VIN vs. V(4) and VIN vs. the current through R1.

.OP - Operating Point

The .OP statement should be used to obtain the DC operating point if no other analysis is run.

Format: .OP

Summary: The inclusion of this line in an input file will force IsSpice4 to determine the quiescent DC operating point of the circuit with inductors shorted and capacitors opened. An operating point is automatically calculated prior to a transient analysis to determine the transient initial conditions, and prior to an AC, noise, or distortion analysis in order to determine the linearized, small-signal models for nonlinear devices. If a transient analysis is run with the UIC option, no DC operating point will be performed unless an AC analysis is run.

Syntax: .OP forces a DC operating point.

The .OP data is listed in the output file.

Getting Output: The operating point voltages for all nodes and voltage source currents are recorded in the output file when a .OP statement is included in the netlist. If no .OP is included, then only the voltages for the top-level circuit nodes will be saved in the output file. The operating point values for voltages, currents, and device/model parameters can also be viewed interactively by accessing the Select Measurements dialog from the IsSpice4 Simulation Control window.

Getting Device/Model Parameter Information
There are two functions, Show and Showmod,

ICL commands like Show and Showmod may be executed from the Simulation Control dialog in the script window.

provide access to the operating point information (SPICE 2 style) associated with devices and models. The Show and Showmod commands are explained in Chapter 11. Appendix B lists all of the device and model parameters that are available. The following example will give the operating point information for the entire circuit.

```
.control    <- beginning of control block
op          <- performs an operating point
show all    <- saves operating point info on all devices
.endc       <- end of control block
```

.TF - Transfer Function

Format: .TF *output input*

Examples: .TF V(5,3) VIN
.TF I(VLOAD) VIN

Summary: The .TF statement produces the value of the DC transfer function between any output node and any independent source, along with the resistance at the input and output.

Syntax: *Output* is the small-signal output variable and can be any node number or name using the format v(#) or v(name). *Input* is the small-signal input independent source.

The .TF data is listed in the output file.

Getting Output: .TF generates output without the need for a .PRINT statement. For the first example, IsSpice4 would compute the DC transfer function ratio of V(5,3) to VIN, the input impedance looking into the circuit at VIN, and the output impedance measured across nodes 5 and 3.

.Nodeset - Initial Node Voltages

Format: .NODESET V(*n1*)=*val1* [...V(*nj*)=*valj*]

Examples: .NODESET V(3)=5V

See Appendix A for more information on solving convergence problems.

Summary: The .NODESET statement is used to specify the node voltage values for the first pass of the DC operating point analysis. The voltage suggestions are then released and the Newton-Raphson iteration process continues to a stable DC solution. The voltage values help IsSpice4 find the DC operating point. This statement may be necessary for convergence on bistable or astable circuits.

Syntax: The .NODESET line defines the voltage nodes and their associated values. The node specification may use any node number or name with the format v(#) or v(name).

.AC - Small-Signal Frequency Analysis

Format: .AC [DEC] [OCT] [LIN] *np fstart fstop*

See the Independent source syntax for more information.

Special Requirement: The AC analysis requires at least one voltage or current source in the circuit to have the AC magval (magnitude value) stimulus. For example: V1 1 0 AC 1.

Examples: .AC DEC 10 1 10K
.AC OCT 10 1K 100MEG
.AC LIN 100 1 100HZ

Summary: This analysis computes a small-signal linear frequency analysis with all nonlinear parameters linearized about the circuit's DC operating point. The magnitude, phase, real , or imaginary values of any voltage, current, or device/model parameter can be recorded.

The AC magnitude value in the voltage/current source statement should normally be set to one.

Syntax: The .AC statement is used to define the frequency band to simulate, as well as the method for recording data. Data may be recorded by octave, by decade, or linearly over the entire spectrum. The recording method is determined by the keyword, DEC, OCT, or LIN, that is specified. Only one keyword may be specified. The number of frequency points is determined by the *np* value. For example, DEC 10 will record 10 points per decade. LIN 100 will record 100 points over the entire frequency span. *Fstart* is the starting frequency in Hz, and *fstop* is the final frequency in Hz.

As stated above, at least one independent source must have the AC keyword. The stimulus magnitude is normally set to 1 so that output variables have the same value as the transfer function of the output variable with respect to the input.

In some cases, such as filter design, it is customary to set the AC magnitude to 2. This is so the combination of the voltage source and matching source impedance deliver a 1 volt magnitude to the circuit.

See the .PRINT statement for more information on postfix notation.

Getting Output: To generate output, the .AC statement must be accompanied by a .PRINT or .VIEW statement. Outputs may be voltages, currents, or device/model parameters. The magnitude, magnitude in dB, phase, real, or imaginary values of these quantities can be recorded using the .PRINT AC statement along with various postfix notation. For example,

.PRINT AC V(5) VDB(5) VP(5) VR(5) VI(5)

will record all the types of data for node 5 vs. frequency. Note: V(5) is equivalent to the SPICE 2 notation VM(5) (magnitude of V(5)). The VM notation is not accepted by IsSpice4. Other combinations can be formed with the ICL Alias function:

```
.control
alias  vmagdiff  mag(v(4) - v(3))              <- magnitude of the voltage difference
alias  realdiv  real(v(4) - v(3)) / imag(v(1))  <- Real(V4,3)/Imaginary(V(1))
.endc
.PRINT AC VMAGDIFF REALDIV                     <- Save the data in the output file
```

Note: Only the magnitude waveforms that are stated in the .PRINT/.VIEW AC statements, and in the ICL view statements, are displayed in real time. The displayed waveforms will be shown with DB scaling, therefore it is not necessary to use the DB notation (VDB(5)).

.Noise - Small-Signal Noise Analysis

Format: .NOISE V(*output* [,*ref*]) *src* [DEC] [LIN] [OCT]
+ *np fstart fstop* [*ptspersummary*]

Note: This syntax differs from that used in previous IsSpice versions.

Special Requirement: The noise analysis requires at least one voltage or current source in the circuit to have the AC magval (magnitude value) stimulus. For example: V1 1 0 AC 1. It is strongly advised that you set the AC magnitude equal to 1, since the analysis is linear and is not affected by source amplitude.

Examples: .NOISE V(5) VIN DEC 10 1kHZ 100MEGHz
.NOISE V(5,3) V1 OCT 8 1.0 1.0E6 1

The noise analysis requires the presence of the AC keyword.

The noise analysis does not require an AC analysis.

Resistors have thermal noise. Semiconductor devices produce shot noise, flicker noise, and burst noise. Capacitors, inductors, and controlled sources are noise-free.

To remove a resistor's thermal noise from the noise calculation set its temperature to -273.15



Summary: The noise analysis calculates the noise contributions from resistors and active devices with respect to an output node voltage. It also calculates the level of input noise from the specified input source, that will generate the equivalent output noise. This is performed for every frequency point in a specified range. A report on the total noise, which is contributed by each noise source, is available in the output file.

Syntax: *Output* is the node at which the total output noise is desired; if *ref* is specified, then the noise voltage (V(*output*)-V(*ref*)) is calculated. By default, *ref* is assumed to be ground. *Src* is the name of an independent source to which the input noise is referred. *Np*, *fstart* and *fstop* are .AC type parameters that specify the frequency range over which the noise data will be calculated, and the number of data points that will be collected. *Ptspersummary* is an optional flag; if included, it causes the total noise contributions of each noise source in the circuit, over the specified frequency range, to be produced.

Note: In SPICE 2, the .NOISE analysis was done in conjunction with the AC analysis. In IsSpice4, the noise analysis does not require a .AC statement. Also in SPICE2, the .NOISE analysis uses an overall circuit temperature value. In IsSpice4, individual part temperatures are used in NOISE calculations, unless option .NOISETEMP is set, in which case the overall circuit temperature is used.

Getting Output: To generate output, the noise statement must be accompanied by a .PRINT NOISE INOISE ONOISE statement. The print statement produces the noise spectral density input and output curves over the specified frequency range. Set *Ptspersummary* to 1 to generate the total noise contributions from each source. All noise voltages/currents are in squared units (V^2/Hz and A^2/Hz for spectral density, V^2 and A^2 for integrated noise) to maintain consistency.

Plots Pop-up: As stated above, two kinds of analyses are performed when a .NOISE analysis is requested; noise spectral density curves and the total integrated noise contributions from each component. Therefore, the Plots pop-up in the Simulation Control window will show two plot entries, one for each analysis.

.Disto - Small-Signal Distortion Analysis

Format: .DISTO [DEC] [OCT] [LIN] *np fstart fstop*
+ [*f2overf1*]

Special Requirement: The distortion analysis requires at least one voltage or current source in the circuit to have either the DISTOF1 or DISTOF2 keywords, or both. If the DISTOF1 or DISTOF2 keywords are missing from the description of an independent source, then that source is assumed to have no input at the corresponding frequency. The default values of the magnitude and phase are 1.0 and 0.0 degrees, respectively. At least one source in the circuit must have the DISTOF# stimulus in order to give the analysis meaning. For example: V1 1 0 DISTOF1 1 DISTOF2 0.01.

Examples: .DISTO DEC 10 1kHz 100MHz
.DISTO OCT 10 1kHz 100MHz 0.9
.DISTO LIN 1 1MEG 100MHz 0.9

Summary: The distortion analysis computes the steady-state harmonic or the inter-modulation products for small input signal magnitudes.

Syntax: The .DISTO statement is used to define the frequency band to simulate, the method for recording data, and the choice between a harmonic or spectral analysis. *Np*, *fstart* and *fstop* are .AC type parameters that specify the frequency range over which the distortion data will be calculated, and the number of data points.

If The F2OVERF1 Value Is Not Present In .DISTO
If the optional parameter *f2overf1* is not specified, .DISTO performs a harmonic analysis i.e., it analyzes the distortion in the circuit using only a single input frequency, F1. The frequency is swept as specified by values in the .DISTO statement exactly as in the .AC statement. More than one input source may have the DISTOF1 magnitude/phase values, but in this case, any DISTOF2 values are ignored. Note: A value of 1 (as a complex

distortion output) signifies Cos(2∗þ∗(2∗F1)∗t) at a frequency of 2∗F1 and Cos(2∗þ∗(3∗F1)∗t) at a frequency 3∗F1. This uses the convention that 1, at the input fundamental frequency, is equivalent to Cos(2∗þ∗F1∗t).

If F2OVERF1 Is Present

If the optional parameter *f2overf1* is specified, .DISTO performs a spectral analysis. The value of *f2overf1* must be a real number between (and not equal to) 0.0 and 1.0. The circuit will be simulated with sinusoidal inputs at two different frequencies, F1 and F2. F1 is swept according to the .DISTO statement options exactly as in the .AC statement. F2 is kept fixed, at a single frequency, as F1 is swept. The value of F2 is equal to (*f2overf1* ∗ fstart). Each independent source in the circuit may potentially have two (superimposed) sinusoidal values for distortion, at the frequencies F1 and F2. The magnitude and phase of the F1 component are specified by the arguments of the DISTOF1 keyword in the independent source statement. The magnitude and phase of the F2 component are specified by the DISTOF2 keyword and associated arguments.

Setting A Value For F2OVERF1

It should be noted that the number *f2overf1* should ideally be an irrational number. Since this is not possible in practice, efforts should be made to keep the denominator in its fractional representation as large as possible, certainly above 3, for accurate results (i.e., if *f2overf1* is represented as a fraction, A/B, where A and B are integers with no common factors, B should be as large as possible). Note that A < B because *f2overf1* is constrained to be < 1. To illustrate why, consider the cases where *f2overf1* is 49/100 and 1/2. In a spectral analysis, the outputs are at F1 + F2, F1 - F2 and 2 ∗ F1 - F2. In the latter case, F1 - F2 = F2, so the result at the F1 - F2 component is erroneous because of the strong fundamental F2 component at the same frequency. Also, F1 + F2 = 2 ∗ F1 - F2 in the latter case, and each result is erroneous individually. This problem is not present in the case where *f2overf1* = 49/100, because F1 - F2 = 51/100 F1 <> 49/100 F1 = F2. In this case, there will be two very closely spaced frequency components at F2 and F1 - F2.

Getting Output: To generate output, the DISTO statement must be accompanied by a .PRINT DISTO statement. If *f2overf1* is not present, the .PRINT DISTO statement will record information about the values of the voltages, currents, and device/model parameters at the 2nd and 3rd harmonic frequencies (2 * F1 and 3 * F1), vs. the input frequency F1. If *f2overf1* is present, the .PRINT DISTO statement produces data for the voltages, currents, and device parameters at the inter-modulation product frequencies F1 + F2, F1 - F2, and (2 * F1) - F2 vs. the swept frequency, F1.

Normally, in the harmonic analysis case, one is interested primarily in the magnitude of the harmonic components, so the magnitude of the AC distortion values are generated by the distortion analysis. It should be noted that these are the AC values of the actual harmonic components, and are not equal to HD2 and HD3 (2nd/3rd harmonic distortion). To obtain HD2 and HD3, you must divide by the corresponding AC magnitude values at F1, obtained from the .AC analysis.

Magnitude, magnitude (in dB), phase, real, and imaginary data formats are all available for both the spectral and harmonic analyses in a manner similar to the AC analysis. For example,

.PRINT DISTO V(5) VDB(5) VP(5) VR(5) VI(5)

will record all of the types of distortion data for node 5 vs. frequency. See the AC and .PRINT sections for additional examples.



Plots Pop-up: As stated above, two kinds of analyses are available when a .DISTO analysis is requested; harmonic distortion and inter-modulation distortion. Therefore, the Plots pop-up in the Simulation Control window will show two or three plot entries, depending on which analysis is run. Inter-modulation distortion produces three plots (f1+f2, f1-f2, and 2f1-f2), harmonic distortion produces two plots (2nd & 3rd harmonics).

Sensitivity Analysis

Format:
```
.control
sens output
sens output ac [dec] [oct] [lin] NP Fstart Fstop
print all
.endc

*#sens output
*#sens output ac [dec] [oct] [lin] NP Fstart Fstop
*#print all
```

Example:
```
.control
sens v(4)
sens v(8) ac dec 1 100k 100meg
print all
.endc
```

Summary: There are two ways to perform sensitivity analysis; with the traditional SPICE method and with Simulation Templates. Simulation Templates are the preferred method and offer significant advantages in output format, analysis support and overall analysis flexibility. For more details on Simulation Templates, including how they work and instructions on how to create your own scripts, please see the on-line help in SpiceNet. The traditional SPICE sensitivity analysis is explained here.

The sens command runs a dc or ac sensitivity analysis. *Output* can only be a node voltage or the current through a voltage source. The first form will produce the DC sensitivity of various component and model parameters to *output*. The second form will produce the AC sensitivity of various component and model parameters to *output*. Output information is produced via the print command. Model and device parameters with zero value are not evaluated during the sensitivity analysis.

Syntax: The sensitivity analysis can be performed for both the DC operating point and for the AC analysis. The sens control

ICL script commands can be entered directly into the Simulation Setup dialog in the schematic.

statement can only be used in its ICL form. There is no “dot” form. Therefore you can run the traditional SPICE sensitivity analysis in one of three ways; from IsSpice4 in the Simulation Control script window, the ICL control block, or as a stand-alone ICL statement. Both of the ICL formats are shown at the start of this section.

Getting Output: The sensitivity analysis must be performed using ICL commands. Therefore, an ICL print statement must also be used. To print the sensitivity with respect to a component value, simply state the reference designation. For an input device parameter, the syntax is ref-des.param_name. For an input model parameter, the syntax is ref-des.m.param_name.

For example:

```
sens v(4)       ; Run DC Sensitivity
print all               ; Data for all device/model parameters
sens v(4) dec 10 1K 100K    ; Run AC Sensitivity
print r1 q1.area q1.m.bf       ; Data for r1 and q1 area/beta
```

The output for the ICL print all function results in three columns of data in the IsSpice4 output file. The columns are: Element name (including the model parameter), Element Value, and Element sensitivity. The list is sorted by the Element name.

Other sorting and output formats are available when using Simulation Templates.

.PZ - Pole-Zero Analysis

Format: .PZ *N1 N2 N3 N4 cur [pol] [zer] [pz]*
.PZ *N1 N2 N3 N4 vol [pol] [zer] [pz]*

Examples: .PZ 4 0 5 0 VOL PZ
.PZ 1 0 3 0 CUR POL
.PZ 2 3 5 4 VOL ZER

Summary: The pole-zero analysis computes the poles and/or zeros of the small-signal AC transfer function from any input to any output.

Syntax: *Cur* stands for a transfer function of the type (output voltage)/(input current) while *vol* stands for a transfer function of the type (output voltage)/(input voltage). These two types of transfer functions cover all of the cases and allow the poles/zeros of functions like input/output impedance and voltage gain to be found. *Pol* stands for pole analysis only, *zer* for zero analysis only, and *pz* for both. This feature is provided because if there is a non-convergence in finding poles or zeros, then at least the other can be found. The input and output ports are specified as two pairs of nodes where *N1* and *N2* are the two input nodes and *N3* and *N4* are the two output nodes.

The PZ option is normally selected to generate both poles and zeros.

Getting Output: .PZ generates results in the output file without the need for a .PRINT statement. For the first example, IsSpice4 will compute poles and zeros of the transfer function between node 4 and node 5.

.Tran - Transient Analysis

Format: .TRAN *tstep tstop* [*tstart* [tmax]] [UIC]

Examples: .TRAN 50NS 1US
.TRAN 10N 10U 9U 1N UIC

Summary: The transient analysis computes the circuit response as a function of time over a user-specified time interval. The initial conditions are normally determined by a DC analysis called the initial transient solution. The UIC option may be used to allow the simulation to begin from a user-specified state.

Data is taken in tstep increments from time 0, or tstart, to the time tstop.

Syntax: The transient time interval and the data printout step are specified on the .TRAN control line. Output data for tabular (.PRINT) and line-printer (.PLOT) output is recorded in *tstep* time increments. *Tstop* is the total analysis time. *Tstart* is an optional alternate starting time. If *tstart* is omitted, data will be recorded starting at time zero. If *tstart* is specified, the circuit is analyzed normally in the interval of [zero to *tstart*], but no outputs are stored. In the interval [*tstart* to *tstop*], the circuit is analyzed and outputs are stored in *tstep* increments. Note, the transient analysis always begins at time zero regardless of the *tstart* value. There is no way to skip from time 0 to a specific time and then begin the analysis.

Tmax is the maximum step size IsSpice4 uses to calculate the circuit response. The IsSpice4 default is (*tstop* - *tstart*)/50.0. *Tmax* guarantees a computing interval (time between internally calculated points) that is smaller than the default. UIC (use initial conditions) is an optional keyword that tells IsSpice4 not to solve for the quiescent operating point before beginning the transient analysis. If this keyword is specified, IsSpice4 uses the values specified using “IC =...” on the various elements as the initial transient condition and proceeds with the analysis. If an .IC line has been given, then the node voltages on the .IC line are also used to compute the initial conditions for the devices.

Integration Algorithm Note: The transient analysis uses Trapezoidal integration as the default method for calculation. Gear integration may be selected via the .OPTIONS Method=Gear parameter.

Getting Output: To generate output, the .TRAN statement must be accompanied by a .PRINT or .VIEW statement. Outputs may be voltages, currents, or device/model parameters. For example,

.PRINT TRAN V(5) @R2[i] @q1[vbe] @M5[id]

would record all the time domain data for node 5, the current through R2, the Vbe voltage of Q1, and the drain current in M5.

.IC - Transient Initial Conditions

Format: .IC V(*N1*)=*val1* ... V(*Nj*)=*valj*

Examples: .IC V(3)=6.8V V(4)=1.25V V(5)=-3.12V

Summary: The .IC statement is used for setting initial conditions for the transient analysis. Note: .IC should not be confused with .NODESET, which is only used to help DC convergence.

Syntax: .IC works two ways, depending on whether or not UIC is present in the .TRAN control statement.

If the UIC statement is present: The transient initial conditions are computed using the specified node voltages. The transient analysis will begin with the specified values. Any IC=value specifications, located on the device call statements, will take precedence over the .IC values.

If the UIC statement is not present: The program solves for the initial transient operating point, using these values as a forced initial condition. The constraints are lifted when the transient analysis is started.

.Four - Fourier Analysis

Format: .FOUR *freq var1* [*var2 ... varn*]

Examples: .FOUR 100KHZ V(4,5) I(VM1)

Summary: The Fourier analysis computes the magnitude, phase, and normalized magnitude and phase, of the DC and first 9 harmonics for each specified output variable. The computational interval is from (*tstop* - period) to *tstop*. Numerical accuracy limits the value of this analysis to rather high values of distortion, usually greater than .1%, which is the default computational accuracy.

Syntax: The value of *tstop* is defined in the .TRAN control statement. Period is computed as 1 / *freq.* The output variables, *var1 ... varn,* are the nodes on which the analysis is performed.

Getting Output: The output of the Fourier analysis is stored in the output file. In order to make sure that any transient residues are removed for the signal, several periods of *freq* should be processed .

Alternate Fourier Analysis: Another more flexible version of the Fourier analysis is available through the use of the ICL Fourier command. Please see Chapter 11 for more information.

.Print - Output Statement

In IsSpice4, *extra voltage sources DO NOT have to be added in order to measure branch currents.*

Format: .PRINT *type var1* [*var2 ... varn*]

The following examples show the different types of data that can be saved in the output file or viewed in real time.

Example: Node voltages, currents, and node names through devices. These may be used with any analysis type parameter.

Node names can be stated as either name or V(Name); Vout or V(Vout).

.PRINT TRAN V(2) V(Vout) @r3[i] @Q1[ICC] @M5[ID] @d2[id]

Example: Device and Model Parameters. These may be used with any analysis type parameter.

.PRINT TRAN @Q1[VBE] @m1[gm] @d1[charge] @r1[p]

Example: For the AC and distortion analyses, the following postfix letters can be added to the V or I variables.

The designation V(#) gives the magnitude of V(#).

Postfix letter	Output	Example
R	real part	IR(V2)
I	imaginary part	VI(10,3)
P	phase	VP(2)
DB	20*log(Magnitude)	VDB(1)

.PRINT AC V(1) VP(1) VDB(1) VR(1) VI(1)
.PRINT DISTO I(V1) IP(V1) IDB(V1) IR(V1) II(V1)

Example: Noise Analysis. The noise print statement only accepts two vectors, inoise and onoise.

.PRINT V(node#,node#) outputs the nodal voltage difference.

.PRINT NOISE INOISE ONOISE

Example: Sensitivity Analysis. The sensitivity analysis must be performed within the ICL control block or script window. Therefore, an ICL print statement must also be used. The syntax for the sensitivity print statement is slightly different than

the normal print statement. As with all ICL print statements, a type parameter is not needed because the print statement applies only to the active analysis. To print the sensitivity with respect to a component value, simply state the reference designation. For an input device parameter, the syntax is ref-des.param_name. For an input model parameter, the syntax is ref-des.m.param_name. For example:

```
sens v(4)              <- DC Sensitivity
print all              <- Sensitivity data for all parameters
sens v(4) dec 10 1K 100K   <- AC Sensitivity
print r1 q1.area q1.m.bf   <- Sensitivity data for r1 and q1
```

Summary: The .PRINT statement selects which voltages, currents, and device/model parameters will be saved in the output file and viewed in real time. Data is saved using a tabular format with columns, which are separated by spaces.

Syntax: The *type* parameter must be one of the following analysis types: **AC, DC, TRAN, NOISE or DISTO**. Output variables begin with a V if they describe a node number, or an I if they describe a voltage source reference designation, or an @ if they refer to a device/model parameters. Output variables may also be node names.

ICL Control Block/Script Window Note: When the .PRINT statement is used in the netlist, vectors for voltages, currents, or device/model parameters are automatically saved and displayed in real time. This contrasts the condition when an ICL print statement, or any other statement that uses a voltage, current, device/model parameter, is used within the control block. In this case, the named vectors must be saved using the save statement, and views must be created with the view statement. For example, .PRINT TRAN V(5) would save and display node 5 in real time. To perform this same function in the ICL control block, use the following:

See Chapter 11 for more information.

```
.control
save v(5)
view tran v(5)
tran 1n 100n
print v(5)
.endc
```

Node Name Note: In the .PRINT statement, node names are specified without any parentheses (VOUT). This is in contrast to other control statements where node names are specified like any other node number (V(VOUT)). Postfix letters can not be used with node names. Node names should not be confused with Alias names, which are created via the ICL alias statement, and used to reduce the complexity of expressions, or ∗Alias statements that are used to associate a user defined name with a node number in the IntuScope analysis program.

Useful parameters include device power, transistor VBE, and FET gm.

Printing Device and Model Parameters
A wide variety of device and model parameters can be stored in the output file and displayed in real time. The available parameters are listed in Appendix B. Parameters come in two types, device and model, and each parameter can be input only, output only, or input and output. Obviously, printing input or input/output parameters is of little value except for verification purposes. Currents through all devices and the power dissipation of all devices is available, including those in subcircuits. No extra voltage sources are needed to measure current.

Be careful not to use alias names that are ICL or IsSpice4 functions or keywords such as Phase, Pulse, Time, Temp, etc.

Printing Aliases
The syntax for printing computed device parameters, subcircuit information, and print expressions can become complex. An ICL alias command is available to reduce these complex phrases to simple, easy-to-remember names. Note: all the alias statements listed below MUST be placed inside the ICL control block or the script window, while the .PRINT statements are located outside of the control block in the input netlist.

Example: Simple Alias examples in a control block

```
control
alias voutput v(5)          <- Alias of a node name
alias vsubnode v(1:X5)      <- Alias of a subcircuit node
alias r1power @r1[p]        <- Alias of a computed parameter
.endc
.PRINT VOUTPUT VSUBNODE R1POWER
```

Important Note: Alias names should be limited to less than 15 characters, which is the limit of the name display in IntuScope.

Print expression data is displayed after the analysis is run.

Printing Expressions
IsSpice4 allows various combinations of voltages, currents and device/model parameters to be combined in mathematical expressions. The expressions can contain the above quantities and may use any of the available math functions described in Chapter 11. These expressions are supported by the ICL alias, let and view commands. However, in order to save the expression, data in the output file, a .PRINT statement is necessary.

Alias statements go in the ICL control block between the .control and .endc lines or in the Simulation Control dialog's script window.

Example: Print Expressions
```
alias vtest (v(4)-v(3)) * V(5)        <- Alias of a node equation
alias stuff v(4) * @r4[i] - @q3[p] <- Alias w/device parameters
alias magdif mag(v(4) - v(3))          <- Alias of AC expressions
alias phdif ph(v(4)) - ph(v(3))      <- Alias of AC expressions
.PRINT TRAN VTEST STUFF
.PRINT AC MAGDIF PHDIF
```

AC Print Note: The data from device/model parameters contains both real and imaginary parts. When used in expressions, the appropriate forms of the vectors should be used throughout. For example, "mag(v(4)) * mag(@r4[i])" will produce a magnitude response, whereas "v(4) * @r4[i]", will produce answers with real and imaginary parts.

See the .SUBCKT statement and Chapter 5 for more information on subcircuit notation.

Printing Subcircuit Data
IsSpice4 allows access to all of the data inside a subcircuit.

Example: Subcircuit Information
```
.PRINT TRAN V(5:X2) V(1:XSUB)        <- Subcircuit voltages
.PRINT TRAN @L1:X2[I] @Q1:X5[ICC] <- Subcircuit currents
```

Real Time Display
Most items in the .PRINT statement are also displayed in real time as the simulation runs. The following items can not be displayed as the simulation runs: phase, real, or imaginary data from the AC and distortion analyses, sensitivity analysis data, and Print Expressions from any analysis. Print expression data will, however, be immediately displayed after the analysis has been run.

.Plot - Output Statement

Format: .PLOT *type var1* [*pl1*, *pu1*]
+ [*var2* [*pl2*, *pu2*]] ... [*varn* [*pln*, *pun*]]

Examples: .PLOT TRAN V(1) 0 1

Summary: The .PLOT statement is used to generate line-printer plots in the output file, using ASCII characters.

Syntax: The .PLOT syntax is the same as the .PRINT syntax for the various analysis types and output variables. The *pl* and *pu* parameters are optional lower and upper plot limits. Automatic scaling is used if *pl* and *pu* are not specified.

Plots that are generated in this manner will not produce tabular data and, therefore, cannot be used by graphics post-processors such as IntuScope.

.View - Real Time Waveform Display

Format: .VIEW *type var1 minvalue maxvalue*

Examples: .VIEW TRAN V(5) 0 10
.VIEW TRAN @R1[I] 0 2
.VIEW AC V(5) -50 20
.VIEW DC I(V5) -.1 .1

The .VIEW statement does not save data in the output file.

Summary: When IsSpice4 runs, waveforms from the .PRINT, .VIEW, and ICL view statements will be displayed as the simulation runs. The progression of the analyses and hence, the waveform display, is: AC, DC, Transient, Distortion, then Noise. All waveforms for which there is a .PRINT, .VIEW, or ICL view statement will be displayed with the limitation that the total number of waveforms will be determined by your screen resolution . All of the distortion analysis products are displayed on one graph.

Syntax: The .VIEW function is used to set the on-screen scaling for a waveform to something other than the default values determined by the .OPTIONS statement. The *type* parameter can be AC, DC, TRAN, NOISE, or DISTO. The *var1* parameter can be a voltage, current, or device/model parameter. The *minvalue* and *maxvalue* determine the graph scaling.

The default scaling for the Transient and DC analyses is ±2V (Node voltages) or ±25mA (Voltage source currents) about the first data point. For AC, Noise and Distortion analyses, the default scaling is ±60dB about the first data point. All AC, Noise and Distortion waveforms are automatically scaled in dB units.

The default scaling values are used for all waveforms that are specified in the .PRINT AC, DC, Disto, Noise or TRAN statements, unless a specific .VIEW statement is present. The default .OPTIONS parameters for the real time waveform display are as follows:

.OPTIONS Parameter	Default	Use
ISCALE	±.025Amps	Current waveforms
VSCALE	±2Volts	Voltage waveforms
LOGSCALE	60 (in dB)	AC waveforms

For example: .OPTIONS VSCALE=5V will set the scaling for all DC and Transient waveforms to ±5V about the first data point.

The .VIEW statement does not support voltage differences, i.e. .PRINT TRAN V(2,3). One node voltage or voltage source current is allowed per VIEW line. The .VIEW AC statement only supports V(#) designations and plots the data automatically in dB. VM(#), VDB(#), phase VP(#) postfix notation are not supported.

The ICL alias command may be used to display the voltage difference. See the Printing Expressions section under .PRINT.

Bad View Syntax Note: The appearance of a blank space on the screen, where a waveform should be, indicates that one of the .PRINT, .VIEW, or ICL view statements has an incorrect node number, node name, or device/model parameter specification.

.Options - Program Defaults

Format: .OPTIONS [option name] [option name=val]
Examples: .OPTIONS ACCT RELTOL=.01
Summary: The .OPTIONS statement is used to set or change various program options.

Syntax: There are two kinds of options: options with a value and options without a value, also known as flags. Flag options can simply be listed on the .OPTIONS line. The options may be listed in any order. In addition, several .OPTIONS statements can be specified in the netlist. The following options are recognized by IsSpice4.

Simulation Parameters

ABSTOL=x Default=1E-12A Example: Abstol=1E-10
Resets the absolute current error tolerance of the program. It is recommended that this value is not altered. However, if currents over 1A are encountered, setting ABSTOL to eight orders of magnitude below the average current can alleviate convergence problems.

ALTINIT=x Default=0 Example: Altinit=1
Causes the initial method used for starting the transient analysis, when the UIC keyword is set, to be bypassed in favor of an alternate algorithm. The alternate algorithm is normally invoked automatically if the initial algorithm fails. You can also set this parameter to a value between 10 and 30. The value corresponds to the exponent of the initial time step used to get the transient analysis started (i.e. Altinit=10 -> 1E-10seconds).

AUTOTOL Default=0 Example:AUTOTOL=2
If AUTOTOL is set larger than 1, then when a node or branch current fails to converge, its tolerance value is multiplied by AUTOTOL. Setting AUTOTOL=2 will rapidly eliminate offending nodes. Smaller values will make the elimination occur more slowly and have a less sever affect. If AUTOTOL is set to less than -1, the same thing occurs using the absolute value of AUTOTOL. The ".OUT" file reports the activity so that you can isolate problem nodes and sources. AUTOTOL is only active for the initial DC operating point calculation.

CHGTOL=x Default=1E-14C
Resets the charge tolerance (in coulombs).

DCCONV
Use this option for circuits that have difficulty with DC convergence.DCCONV sets the following values: ramptime = 10e-9; rshunt = 100 meg.

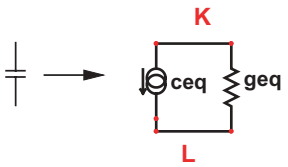
GMIN=x Default=1E-12Ω^{-1}
Resets the value of GMIN, the minimum conductance used in any circuit branch.

Use ICSTEP to correctly initialize digital behavioral circuits for DCOP and AC analysis.

ICSTEP=x DEFAULT=40 Example:ICSTEP=10
GEQFREQ=x DEFAULT=1e12 Example:GEQFREQ=1p
DC Convergence in SPICE simulators cannot be achieved for analog feedback circuits where high gain amplifiers are cascaded and with active regions that are offset. These circuits work perfectly in practice, however, today's standard SPICE convergence algorithms tend to oscillate and find a solution only by lucky chance. This is due to the chaotic nature of the numerical oscillation process. In practice, such circuits do not oscillate in the time domain because capacitors are used to dampen the oscillation in accordance with control system theory.

ICSTEP allows you to retain bistable models in your AC analysis and use capacitor ICs to initialize the circuit state.

The ICSTEP convergence algorithm was implemented to solve this type of problem. In this algorithm, each capacitor that has an Initial Condition (IC)=xxx will have a conductor in parallel with a current source placed across it. The current, ceq is the product of the IC voltage and the conductance, geq. The conductance starts off very high and is stepped down toward zero for each successful iteration. At the final iteration, ceq and geq are set to zero. It's probably easier to visualize it using a Thevenin Equivalent consisting of a resistor in series with a voltage source. But the Norton version slips directly into the SPICE admittance matrix as shown below.



geq	-geq	K row	ceq
-geq	geq	L row	ceq
K col	L col		

The following IsSpice4 options control this algorithm:
.OPTION ICSTEP = [num]
.OPTION GEQFREQ = [omega]

where num is a value between 1 and 100 that sets the number of steps and omega is an effective radian frequency, it defaults to 1e12 if you don't set it.

The initial geq is set to the product of GEOFREQ * CapValue and ceq = geq*InitCapVoltage.

ITL1=x Default=100 Example: Itl1=300
Resets the limit to the number of DC Newton-Raphson iterations that IsSpice4 will perform before declaring "No convergence in DC analysis". If this limit is reached without convergence, IsSpice4 will automatically invoke the built-in Gmin stepping and Source Stepping algorithms to achieve convergence. Setting ITL1 to 300 can help to achieve DC convergence if a failure occurs.

ITL2=x Default=50 Example: Itl2=100
Resets the DC transfer curve iteration limit to the number of DC Newton-Raphson iterations that IsSpice4 will perform at each step of the sweep before declaring "No convergence in the DC sweep analysis." Setting ITL2 to 100 can help the .DC analysis to converge if a failure occurs.

ITL3 and ITL5 are no longer used in IsSpice4.

ITL4=x Default=10 Example: Itl4=100
Sets the number of steps for each transient time point. Setting ITL4 to 100 can help solve "Time step too small" errors in the transient analysis.

ITL6=x Default=10 Example: Itl6=100
Sets the number of steps for the source stepping DC convergence algorithm. Source stepping is automatically invoked if the Gmin stepping algorithm fails. Therefore, it should not be necessary to change this value. This option is called "Gminsteps" in SPICE3 programs.

MAXORD=x Default=2 Example: Maxord=6
Sets the maximum order for integration if the Gear integration method is selected. The value must be between 2 and 6.

METHOD=Gear Default=TRAP
Placing Method=Gear on the .OPTIONS line causes IsSpice4 to use Gear integration. Trapezoidal integration is used if Gear is not specified.

Minbreak speeds up Transmission line simulations.

MINSTEP=x Default=none Example: MINSTEP=1n
The value of MINSTEP is used as the minimum time at which the internal data is accumulated during a simulation. Since the internal data is determined by the activity of the circuit and not the .TRAN statement, the "snap" turn off of a diode during a power simulation can cause data to be collected at frequencies that are much higher than the frequency of interest. MINSTEP is used to reduce the extraneous data collected internally and reduce the amount of memory used by a simulation. When setting MINSTEP, note that the higher frequency data will be folded into the new sampling interval and appear as lower frequency oscillation.

Try using MINBREAK=-1 to reduce memory use if you are <u>not</u> using transmission lines.

MINBREAK=x Default=off Example: Minbreak=5N
Sets the minimum time between transient breakpoints. Minbreak is used to speed up the simulation of circuits that contain ideal transmission lines. Increasing the minbreak time will speed up the simulation at the expense of accuracy. For adequate accuracy and best speed, it is recommended that the minbreak value be set to about 1/4 of the time of the smallest transmission line delay. The method used to simulate circuits using ideal transmission lines has been completely changed from the process used in SPICE 2. The result is greatly increased speed and much smaller memory usage. The minbreak value can be used to further increase the speed of the analysis.

*If MINBREAK is set to -1, IsSpice4 will not save any time information prior to the value set for TSTART on the .TRAN line. For long delayed simulations, this will reduce the amount of memory used by a simulation. If the simulation contains transmission lines, this parameter should not be used.

MULTITHREAD=x Default=1 Example: Multithread=2
The number of multithreaded circuits.

NOISETEMP Default=off Example: Noisetemp
If .NOISETEMP is set, then overall circuit temperature is used in noise calculations. Otherwise, each part's individual temperature is used in the NOISE calculation.

NOOPITER Default Flag State=Off
Causes the simulation to go directly to gmin stepping and bypass the standard operating point routine.

NUMDGT=x Default=6 Example: Numdgt=9
Controls the number of digits after the decimal place for data that is stored in the output file.

PARAMDIGITS=x Default=2 Example: PARAMDIGITS=12
Option that is only active in ICAPS parameter passing and will set the number of significant digits that will be printed on the netlist for a passed parameter/value.

PIVREL=x Default=1E-3
Resets the relative ratio between the largest column entry and an acceptable pivot value.

PIVTOL=x Default=1E-13
Resets the absolute minimum value for a matrix entry that is accepted as a pivot.

RELTOL=x Default=.001 Example: Reltol=.01
Resets the relative error tolerance of the simulation. The default value is 0.001 (0.1 percent). This is the most important parameter for control of the simulation accuracy. It is recommended that RELTOL be set to no larger than .01. Use of the .01 value is recommended in order to speed up the simulation. Results should not be noticeably affected.

RSHUNT Default=Off Example: RSHUNT=1MEG *
When entered, this value is used as a shunt resistance to ground from every analog node.

RAMPTIME=x Default=0 Example: Ramptime=10u *
The time that is used to ramp the supply voltage for a transient analysis. This parameter can be useful for aiding convergence for circuits that are initially unstable, by realistically modeling the turn-on time of power supplies.

TRANCONV
Helps with transient convergence. Use to avoid time step too small errors. TRANCONV sets these values: abstol = 50 µ; vntol = 50 µ ; reltol = 0.01; and method = gear

TNOM = x Default=27°C Example: Tnom=0
Resets the temperature at which model parameters were calculated. Any TNOM values that are stated in .MODEL statements will override this value.

TEMP = x Default=27°C Example: Temp=75
Sets the temperature at which the entire circuit will be simulated. Any temperature values that are specifically stated on an element will override this value.

TRTOL = x Default=7
Resets the transient error tolerance. The default value is 7.0. This parameter is an estimate of the factor by which IsSpice4 overestimates the actual truncation error. It is recommended that this value is not changed.

TRYTOCOMPACT Default Flag State=Off
Applicable only to the LTRA model. When specified, the simulator tries to condense a lossy transmission lines' past history of input voltages and currents.

VNTOL=x Default=1E-6 Example: Vntol=1E-4
Resets the absolute voltage error tolerance of the program. The default value is 1 µvolt. It is recommended that this value is not altered. However, if voltages over 100V are encountered, setting VNTOL to eight orders of magnitude below the average voltage can alleviate convergence problems.

VSECTOL=x Default=0 Example: Vsectol=1E-9
Reduces the time step when the volt-second product described by its argument is exceeded by the current time step, times the predicted voltage minus the iterated voltage. The test is made for all nodes. Use this option when the automatic time step isn't scaling back the time step when behavioral switching events occur.

Mixed-Mode Options

NOOPALTER=x Default Flag State=On
Causes analog/event alternations during a DC operating point to be disabled.

AUTOPARTIAL=x Default Flag State=Off
Causes the partial derivatives for each code model to be computed by IsSpice4. Typically, you will provide the partial derivative computation in the code model and leave this option off in order to increase the speed of computations.

MAXOPALTER=x Default=300 Example: Maxopalter=500
Maximum number of analog/event alternations for a DC operating point before nonconvergence is reported. The default value of this option is determined by the circuit and depends on the number and type of code models present.

MAXEVTITER=x Default=300 Example: Maxevtiter=500
Maximum number of event iterations for each analysis point before nonconvergence is reported. The default value of this option is determined by the circuit and depends on the number and type of code models present.

CONVLIMIT=x Default Flag State=Off
Enables convergence assistance for code models.

CONVSTEP=x Default=0.25 Example: Convstep=.1
The fractional steps allowed by code model inputs between iterations.

CONVABSSTEP=x Default=0.1 Example: Conabsvstep=.05
The absolute steps allowed by code model inputs between iterations.

Model Options

BADMOS3 Default Flag State=Off
Causes the old SPICE 3E version of the MOS3 model, with the "kappa" discontinuity, to be used.

BYPASS Default Flag State=On
The implementation of the inactive device bypass algorithm found in SPICE 2 programs has been greatly improved in IsSpice4. Inactive device bypass is a technique that is used to speed up a simulation by reusing the terminal conditions of devices that have not changed significantly during the past evaluation period. Turning the device bypass off will slow down the simulation, and is therefore not recommended.

CML=x Default=none
Sets the path to the named code model DLL file.

DEFAD=x Default=0
Resets the value for MOS drain diffusion area. The parameter in the MOSFET M element statement is AD. This statement will cause the value of AD to have a default value other than 0.

DEFAS=x Default=0
Resets the value for MOS source diffusion area. The parameter in the MOSFET M element statement is AS. This statement will cause the value of AS to have a default value other than 0.

DEFL=x Default=100µm
Resets the value for MOS channel length. The parameter in the MOSFET M element statement is L. This statement will cause the value of L to have a default value other than 100µm.

DEFW=x Default=100µm
Resets the value for MOS channel width. The parameter in the MOSFET M element statement is W. This statement will cause the value of W to have a default value other than 100µm.

OLDLIMIT Default Flag State=Off
Use SPICE 2 MOSFET limiting

Screen/File Output Options
ACCT Default Flag State=Off
The ACCT flag is used to produce a summary listing of accounting and simulation related information. The data is stored at the end of the output file. Information highlights include: operating temperature, number of iterations for various operations, and simulation time for various analyses.

INTERPORDER=x Default=1 Example: Interporder=2
Sets the interpolation order, which is used for the calculation of data from the raw internal IsSpice4 data.

ISCALE=x Default=.025Amps Example: Iscale=1
Sets the default scaling for current waveforms displayed in the IsSpice4 real-time view graphs.

LIST Default Flag State=Off
The LIST option causes the actual netlist, simulated by IsSpice4, to be placed in the output file. This netlist may be different than the user-generated netlist. The subcircuits will be flattened and any SPICE 2 polynomial syntax for the E, F, G, or H elements will be translated into B elements.

LOGSCALE=x Default=60 (in dB) Example: Logscale=20
Sets the default log scaling for AC waveforms, which are displayed in the IsSpice4 real time view graphs.

VSCALE=x Default=2Volts Example: Vscale=15
Sets the default scaling for voltage waveforms that are displayed in the IsSpice4 real time view graphs.

Boolean Options
LONE = x Default=3.5 Example: Lone=5
Sets the value for the logic 1 state, which is used in the analog behavioral element (B) with boolean expressions. When a boolean expression is evaluated as true (logic 1), the output of the B element will be this value.

LZERO = x Default=.3 Example: Lzero=0
Sets the value for the logic 0 state, which is used in the analog behavioral element (B) with boolean expressions. When a boolean expression is evaluated as false (logic 0), the output of the B element will be this value.

LTHRESH = x Default=1.5 Example: LTHRESH=2.5
Sets the value for the logic threshold, which is used in the analog behavioral element (B) with boolean expressions. Below this voltage level, a voltage will be evaluated as a zero. Above this level, a voltage will be evaluated as a one.

Changes From SPICE 2
The following parameters are not recognized by IsSpice4: **ITL5** (The transient analysis total iteration limit is unlimited in IsSpice4), **LIMPTS** (There is no programmed default ceiling to the number of data points that IsSpice4 will save), **LVLTIM** (The transient algorithm, which uses iteration control, is not implemented in IsSpice4), **NOMOD**, and **NOPAGE**.

Analyses At Different Temperatures

Format: .OPTIONS TEMP=tempval

Example: .OPTIONS TEMP=50 TNOM=0
.MODEL QMOD NPN (TNOM=10)
Q1 1 2 3 QN2222 TEMP=75

See the individual device syntax for more information on temperature-related parameters.

Summary: Temperature effects are built into the behavior of all active elements. Resistors can be made temperature dependent if temperature coefficients are inserted into a resistor .MODEL statement. To simulate a change in temperature for the entire circuit, a new temperature can be placed on the .OPTIONS line via the TEMP parameter. To simulate a change in temperature for an active element or a resistor, simply state the temperature on the device call line. Note, you may need to adjust certain temperature related parameters in some device models. See the device's model parameters for more information.

Syntax: All input data for IsSpice4's model parameters is assumed to have been measured at a temperature of 27°C unless it is globally changed for all models via the .OPTIONS TNOM parameter, or locally changed for a single model via the .MODEL TNOM parameter. The circuit simulation is performed at a temperature of 27°C unless it is globally changed via the .OPTIONS TEMP= parameter, or locally changed on a single element via the TEMP= specification.

Simulating At Multiple Temperatures
The simplest method for performing temperature sweeps is by using the Alter tool and associated dialog in the schematic. Please see the on-line help or the Getting Started manual for more information on the Alter function.

Modifying the circuit temperature via the .OPTIONS TEMP value is different than the method used in SPICE 2 based simulators. Use of the single .OPTIONS TEMP value replaces the SPICE 2 syntax, which used a separate .TEMP statement.

See the Analysis control section in Chapter 11 for an explanation of running analyses at different temperatures using ICL scripts.

Getting Output: After the temperature is set, either on an element or for the whole circuit, the analysis results will be produced in the same manner as usual except that the specified temperature effects will be included.

Title and End Statements

Format: .END
Examples: ANALOG BICMOS ASIC
Test Circuit For Power Supply

The title line must be the first line in the input file. In IsSpice4, there can only be one title line and one complete circuit description in a file. The .END statement is the last in the circuit definition.

Continuation and Comment Lines

Examples:
```
.MODEL QN2222 NPN
+ (BF=150 IS=1E-12)
*Subcircuit connections are ....
R1 1 0 10K  ; Snubbing resistor
```

Continuation lines begin with a + sign in the first column. The contents of the line are appended to the line directly preceding the continuation line. Comments are used to document various aspects of the circuit netlist. They may be included anywhere in the netlist.

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References

Interactive Command Language

Important Note: This chapter is an introduction to ICL Scripting. Complete help on Simulation Templates, plus all ICL functions and commands, is available from the on-line help system in SpiceNet and IsSpice4.

ICL Defined

ICAP/4's Interactive Command Language (ICL) is a SPICE 3 language extension that enhances the abilities of traditional Berkeley SPICE. It provides a set of commands and functions for advanced interactive and batch-style control of the simulator, and special waveform processing in the IntuScope waveform viewing tool.

The ICL enables simulation breakpoints, parameter value changes, print aliases and expressions, computed model parameters, and control loops to be used in simulation. Simulation scripts, or test procedures, combining any number of these commands can also be created. For instance, the ICL stop statement can be used in monitoring if the power in a device has exceeded a value. If so, the simulation is stopped and a corresponding message posted.

ICL commands can be inserted directly into the IsSpice4 Simulation Control dialog's Script window, Expression window, or Command window, and into the netlist inside a control block. The control block is placed at the top of a standard IsSpice4 netlist after the title, and before any "dot" analysis statements. The control block is a section of the netlist reserved for ICL commands. It begins with the line ".control," and ends with the line ".endc." Single-line ICL commands can also be inserted in the netlist by placing the *# characters at the beginning of the line. The .control and .endc lines are not needed when ICL commands are used directly in IsSpice4.

All output generated by ICL statements (print, show, etc.) in the Script, Expression, and Command windows is directed to the IsSpice4 Output window. All ICL statements in the input netlist generate output in the output file.

Contrary to the traditional SPICE syntax, execution of ICL statements is ORDER DEPENDENT.

Simulation Breakpoints and Control Loops
The ICL provides a new dimension in analysis with the introduction of *Simulation Breakpoints*. Breakpoints are commands that can be set for any type of simulation to monitor circuit behavior. The simulation will halt when the breakpoint condition is satisfied. Breakpoints are set with the STOP command. The STOP command accepts a vector expression as an argument and continuously evaluates the expression during the simulation. When the argument evaluates true, the simulation halts. A simple example is;

```
stop when v(7) > 4.5
```

In this case, the simulation will stop when the voltage at node 7 exceeds 4.5 volts.

In addition to the STOP command, control loops are available that allow multiple simulations to be performed. With the control loops, circuit behavior can be monitored, circuit parameters varied, and simulations rerun, all during a single simulation session.

Output commands executed from the IsSpice4 Script window direct output to the IsSpice4 Output Window.

Simulation Output
Output for expressions containing any node voltage, current, or device/model parameter can be displayed and recorded. For example, a node difference can be obtained by simply stating

```
alias  vdiff  v(1)-v(2)
```

The alias name can then be used in the standard .PRINT command to obtain the desired output in the output file.

View and let commands are available to allow parameters or expressions to be viewed in real time, but not printed or saved to the output file. This allows a parameter to be investigated without increasing the memory needed to create the output file.

Model Parameter Output
The show and showmod commands produce operating point information for devices and models.

The Interactive Command Language

ICL commands can be placed in the Script, Expression, or Command windows, or between the .control and .endc statements. A simplified control block in the input netlist is;

Each netlist may only contain one control block.

```
.control
... commands
.endc
```

Important Note: .control and .endc statements are only required for an ICL control block in the input netlist. They are NOT required for the Script, Expression, or Command windows. The control block should be positioned at the beginning of the IsSpice4 input file description.

Individual ICL statements can also be put into the input netlist by placing a *# in front of them. For example.

```
*#OP
*#sens V(4)
*#print all
```

Order Dependency
ICL commands are position sensitive because they are executed in the order as they are encountered. In general, commands should be issued in the following order;

Save vectors
Alias statements
View statements
Stop, Breakpoints or Control Loops
Analysis control statements
Let statements
Alter statements
Output statements

A more detailed treatment of the control block is provided in the "Using the Control Block" section later in this chapter.

Vectors

Data is saved in the form of vectors. Vectors are generated with the save, alias, let or .PRINT commands. This will create a vector for use as an argument in future ICL commands, and/or to print output data in an IntuScope compatible format.

TIME and FREQ are reserved vector names and represent the default time and frequency vectors for the last analysis.

The save, alias, and let commands are used to create vectors for simulation control command arguments. They are also used to save vectors for schematic cross-probing and display in IntuScope.

Vectors may be assigned to a previously defined vector, floating-point number (scalar), or list such as [P1 P2 ... Pn], which is a vector of length n. A number may be written in any format acceptable to IsSpice4, such as 14.6MEG or -1.231E-4.

A vector name beginning with the '@' symbol is a reference to an internal device or model parameter. If the vector name is of the form @*name*[*param*], *name* must be a device reference designation, and *param* must be a valid parameter for the specified reference designation. Appendix B lists all available device and model parameters. You can also use this notation:

param (name). For example i(ri) is the same as @ri[i].

Vectors are referenced by their names. To reference items within a vector, the following syntax is used:

vec[n] or vec[m, n]

The linearize command converts data onto a uniform time scale.

The first notation refers to the nth element of *vec*. The second notation refers to all of the elements of *vec* that fall between the mth and the nth element, inclusive. If n is less than m, the order of the elements in the result is reversed.

All data in the output file is accompanied by an index column that represents the location of each data point in the output vector. For the AC and DC analyses, and their associated sub-analyses, all data is directly related to the analysis control statement. Hence, to find a location, simply use the analysis

control parameters to calculate the position, or refer to the index column from a previous simulation. For a transient analysis, all vectors contain data according to a dynamic time scale. This time scale will contain more data in the transition locations and less data in other areas. When the vector is printed, all values are linearized onto a uniform time scale based on the TSTEP value. Note: a vector must be linearized (with the linearize command) before data can be accessed via an index.

For expressions that return a vector, the notation expr [n m], where n and m are numbers, denotes the range of elements from expr between n and m. The notation expr [n] denotes the nth element of expr. If m is less than n, the order of the elements in the vector is reversed.

Functions

There are two types of functions; predefined or user-defined macros. Function arguments may be scalar or vector quantities.

There should be no spaces before or after the > or < signs. Use of the synonyms ge and le is recommended.

Macros are defined with the function command. For example;

```
function max(x,y) (x > y) * x + (x <= y) * y
function min(x,y) (x < y) * x + (x >= y) * y
function sdev(vec) sqrt(mean(vec*vec) - mean(vec)^2)
```

The macro “max(x,y)” accepts the scalar arguments x and y and returns the larger value. The arguments x and y can be scalar or vector quantities. For example,

```
larger = max(v(8),v(7))
```

The functions max(x,y) and min(x,y) produce maximum and minimum vector envelopes if x and y are vectors.

In general, all operations and functions will work on either real or complex values. However, operations such as the logarithm of a negative number, will yield errors. All functions and operations operate point-wise on their arguments unless otherwise described. Hence, where appropriate, the argument (arg) can be either a vector or a scalar.

The complete set of functions, including their description and format, is available in the on-line help and on the Intusoft web site. A brief description is available in the next section.

Trigonometric functions will treat arg as radians unless the variable "units" is set to degrees. See the SET function for more details.

Function	sin(3.1415)	norm(v(8))
Examples:	mag(v(3)+v(2))	exp(@r2[i])
	sqrt(v(34))	deriv(V(3))

Expressions

Expressions are used to produce information to make a decision or calculate vector output that is not otherwise readily available from the simulation. An expression may consist of any combination of vectors, scalars and functions. The equations and functions can be constructed using any combination of the following operators: +, -, *, /, ^, % and ,.

% The modulo operator. The result is the remainder when the first number is divided by the second. Note that both arguments are rounded down to the nearest integer before the operation is performed.

, The comma operator has two meanings: if it is present in the "argument list" of a function, it serves to separate the arguments. When used in the term x, y, it is synonymous with x + j(y). Such a construction may not be used in the argument list to a macro function. For example;

Functions can be used in any ICL statement.

3,5 = 3+j5
max(3,5) determines the larger of 3 or 5

Logical operations

symbol	definition
&	and
|	or
!	not

Relational operations

symbol	synonym	definition
<	lt	less than
>	gt	greater than
>=	ge	greater than or equal
<=	le	less than or equal
=	eq	equal
<>	ne	not equal

Logical and relational operators are available for constructing expressions in breakpoints, control loops, and If-Then-Else statements. When used in an algebraic expression, they work as they do in the C programming language, and produce values of 0 or 1.

and or & - 1 if both operands are nonzero, 0 otherwise.
not or ! - 1 if the operand is 0, 0 otherwise.
or or | - 1 if either of the two operands is 1, 0 otherwise.

Relational operators can be substituted for the synonyms listed beside them. These synonyms are useful when the symbols such as < and > become confused with IO redirection, such as in the max function example.

Examples:

```
while mean(v(5)) > 45m & mean(v(4)) > 45m
if v(4) <= @r3[i]*@r3[resistance]
```

Note: The "=" operator should not be used with the stop command. This comparison should only be made with values that can truly be equal. Data points calculated during a transient simulation are a discrete set of numbers that are unlikely to ever be exactly equal to a predefined value.

Variables
Additional information used for simulation control is obtained through the use of variables. There are many variables that have a special meaning to IsSpice4. A variable is manipulated with the ICL "set" command. All predefined variables are listed under the set command. In addition to the variables listed, all .OPTIONS parameters are considered variables and can be changed with the set command.

Examples:

```
set temp=125          set global circuit temperature to 125°C
set units=degrees     set trig function units to degrees
print $temp $units    print the variable values
```

ICL Function Summary Listing

See the on-line help for complete information and details on ICL Scripts and Simulation Templates.

Mathematical Functions
Arg may be a scalar or a vector.

abs(arg) - The absolute value of arg.
db(arg) - Decibels (20.0 * log base 10 of arg).
ceil - Returns the ceiling of the vector.
ddt(arg) - Time derivative of arg
deriv, differentiate (arg) - Calculates the derivative of the vector with respect to the current plot scale. (The derivative uses numerical differentiation by interpolating a polynomial of "polydegree" order. If polydegree, a set variable is not set, the order defaults to 1.) May also be written as differentiate(vec).
exp(arg) - e to the arg power.
floor - Returns the floor of the vector.
im, imag(arg) - Returns the imaginary part of a complex vector in a real vector. May also be written as im(vec).
j(arg) - arg multiplied by sqrt(-1).
ln(arg) - The natural logarithm (base e) of arg.
log(arg) - The logarithm (base 10) of the arg.
mag, magnitude (arg) - Returns the magnitude of a complex vector in a real vector. May also be written as magnitude(vec.
ph, phase (arg) - Returns the phase of a complex vector in a real vector (expressed in degrees). May also be written as phase(vec).
pulse - Returns a vector that is the length of the default vector that is unit for the number of points in its argument and zero thereafter.
re, real(arg) - Returns the real part of a complex vector in a real vector. May also be written as re(vec)
rnd(arg) - Returns a value equal to a random number between 0 and the corresponding element of the argument.
sqrt(arg) - The square root of arg.
vector(arg) - Returns a vector consisting of the integers from 0 up to the magnitude of its argument.

Trigonometric Functions

atan(arg) - The inverse tangent of arg.
cos(arg) - The cosine of arg.
sin(arg) - The sin of arg.
tan(arg) - The tangent of arg.

Cursor Relative Functions

These functions evaluate the vector between cursor 0 and cursor 1, or utilize one or more of the cursors.

getcursorx - Returns the value of the cursor (x-axis scale).
getcursory - Function with 2 arguments, vec and cursor number returns the value of the vector identified by the cursor number.
getcursory0 - Returns the vector value corresponding to cursor 0 for vector (v(1)).
getcursory1 - Returns the vector value corresponding to cursor 1 for vector (v(1)).
max - Maximum value.
mean, average - Average value, by integration.
min - Minimum value.
pk_pk - Peak to peak.
rms - Root mean square.
stddev - Standard deviation (rms with average removed).
tfall - The 10-90% transition using cursor 0 and cursor 1 to define initial and final value.
trise - The 10-90% transition using cursor 0 and cursor 1 to define initial and final value.

Vector Functions

The following functions require a single vector argument except as noted.

alias⬧ - Generates an alias name for vector or vector expression.
diff⬧ - Compares vectors from different plots.
display⬧ - Prints a summary.
finalvalue - The last value of a vector.
initialvalue - The initial value of a vector.
interpolate - Rescales a vector from another plot to the current plot.

See the on-line help for complete information and details on ICL Scripts and Simulation Templates.

isdef	- Returns 0 if the argument is not a vector, else returns 1.
length	- Returns the length of the vector.
nextplot	- Enumerates a plot list.Tthe first plot's vector is returned; if the argument is null, null is returned at the end. The return value is an alias to the plot scale. You should not use plot the resolution operator, plot.pl, for this vector.
nextvector	- Enumerates a vector list; the first vector is returned if the argument is null. Null is returned at the end. The return value is an alias to the vector. If you use the plot resolution operator, refplot.nv, then you will enumerate the refplot vectors.
norm	- The elements of the argument are all multiplied by the inverse of the largest argument (i.e., the largest magnitude will be 1).
operatingpoint	- Returns the magnitude of the first element.
phaseextend	- Extends phase past +-180 degrees, and assumes the initial phase is within the +-180 degree boundary.
pos	- Returns a vector whose values are 1 if the corresponding element of the vector has a non-0 real part, and 0 otherwise.
sameplot	- Returns 1 if a vector is in the current plot.
unitvec(arg)	- Returns a vector consisting of all 1s, with length equal to the magnitude of the argument.

ICL Command Summary Listing

Output Commands

The following commands are used to produce output.

header	- Prints header information to the XSPICE code model interface.
nopoints	- Removes reference points previously placed on one or more plots by the points command.
points	- Places data points on the IsSpice4 screen.
probe/csdf	- Prints vectors in a CSDF style output.
save	- Saves a vector for later use.

sendplot - Displays a vector in IntuScope.
show - Prints out operating point information for models.
showmod - Prints out model parameter information.
view - Assigns a vector to a real time view window.
write♦ - Writes raw data to a file.

Analysis Commands
All of the standard SPICE analysis commands (AC, DC, TRAN, NOISE, DISTO, SENS, etc.) are available in the ICL.

ac - Performs an ac analysis
dc - Performs a dc sweep analysis
disto - Computes the steady-state harmonic (no f2overf1 value) or intermodulation products
fftinit♦ - Initializes the FFT sin/cos table for a 2^radix data length.
filter♦ - Filters a vector by numpoints using a triangular shaped weighted average.
fourier - Performs a fourier analysis.
freqtotime♦ - Performs a fourier transform from frequency to time.
noise - Performs a noise analysis.
op - Determines the operating point of the circuit.
poly♦ - Calculates polynomial coefficients for best fit to the specified vector.
pwl♦ - Makes SPICE-compatible piecewise linear listing in the output window.
pz - Finds the pole and zeros of an ac transfer function.
rotate♦ - Rotates a vector by numpoints, left if numpoints is negative.
sens - Performs an ac or dc sensitivity analysis.
tf - Performs a transfer function analysis.
timetofreq♦ - Performs a fourier transform from time to frequency.
timetowave♦ - Performs an in place wavelet transform using daub4 wave function.
tran - Performs a time domain analysis.
wavetotime♦ - Performs an in place inverse wavelet transform using daub4 wave function.
wavefilter♦ - Sets all values of the vector less than the limit to zero.

♦ Used in IntuScope.

Simulation Commands

The commands in this section control the simulation flow. The breakpoint command can accept vector-based arguments. These arguments can be simple comparisons or complicated expressions.

delete	- Deletes a specified breakpoint.
freqtotime	- Performs a fourier transform from frequency to time.
quit	- Terminates a simulation.
resume	- Continues a simulation after a stop.
runs	- Runs a script that was previously saved.
status	- Displays the currently active breakpoints and traces.
step	- Iterates the simulation n number times, or once.
stop	- Sets a simulation breakpoint.
where	- Identifies a problem node or device.

Vector Commands

The following commands are used to operate on vectors.

alias♦	- Generates an alias name for vector or vector expression.
copy♦	- Copies a vector to the current plot, interpolating all vectors in the current plot.
destroy♦	- Throws away all the data in the plot.
diff♦	- Displays the difference between the vectors from two different simulations.
display♦	- Outputs a list of the currently available vectors.
function♦	- Defines a function.
functionundef♦	- Un-defines a function.
let♦	- Produces a new vector from an existing vector or expression.
linearize♦	- Formats transient vector data onto a linear scale.
nextplot	- Returns an alias for the scale of the next plot or null if no more plots.
sort	- Sorts vectors by name or value in ascending or descending order.
unalias	- Removes an alias
unlet♦	- Removes a let.

♦ Used in IntuScope.

Circuit Commands

The following commands can be used inside or outside a control loop to change the value of a component or model parameter.

alter - Changes a component or model parameter value.
alterparam - Alters parameter value by the expression value.
echo♦ - Stores text in the output file.
listing♦ - Prints the input netlist.
load♦ - Loads data, previously stored using write.
nameplot♦ - Changes the name of the current plot.
newplot♦ - Creates a new plot with a default scale [optional copy]
nextparam♦ - Selects next parameter with tolerance, if null gets first one with tol.
runs♦ - Runs a script that was previously saved.
rusage - Outputs current resource usage information.
set♦ - Changes the value of the word given, i.e., filetype, fourgridsize, nfreqs, nobreak, noasciiplotvalue, noprintscale, polydegree, printmode, rewind, spicedigits, units, width and colwidth below.
colwidth♦ - Controls the column width for printtext.
filetype♦ - Controls the write command file format.
fourgridsize♦ - Number of points in the fixed grid used for interpolating when performing Fourier analysis in the control block.
noasciiplotvalue♦ - Don't print the first vector plotted to the left when doing an ASCII plot.
nobreak♦ - Print continuous ASCII output plots without page break.
nfreqs♦ - The number of frequencies to compute in the Fourier analysis (Defaults to 10).
noprintscale♦ - Don't print the X-axis scale in the leftmost column when printing tabular data.
polydegree♦ - The degree of the polynomial that the Fourier command uses.
printmode♦ - Changes the behavior of the print command.
rewind♦ - Sets the output file pointer to the beginning of the file so that the input netlist and other information is not included.

♦ Used in IntuScope.

spicedigits♦ - Sets the scientific data precision used for printout and display.
units♦ - If this is set to “degrees,” then all trig functions will use degrees. Otherwise, radians are used.
width♦ - Sets the width of the page used for the tabular int data and ASCII plots.
setparam - Sets the current parameter.
setplot♦ - Sets the currently active plot of the plot with the given plotname.
unalterparam♦ - Restores parameter value to the nominal value.
unset♦ - Clears a variable.
version - Prints the version number.

Control Loop Commands

Control loops are used to perform a series of analyses. All loops require an end statement. The control loop commands can accept vector-based arguments. These arguments can be simple comparisons or complicated expressions. Any combination of analysis, circuit, and control loop commands can be grouped together in a script to perform multiple simulations.

break♦ - Breaks out of a block function.
continue - Continues a loop to the next argument.
dowhile♦ - Executes the statements between the dowhile and end lines while the condition is true; the condition is tested after the loop is executed.
else - Goes with the if command.
end♦ - Ends a clock function.
foreach♦ - Does the commands between the foreach and the end lines, once for each value listed.
goto♦ - Goes to a label.
if♦ - Executes the (...commands...) if the condition is true.
If-Then-Else♦ - Allows a decision to be made.
label♦ - Creates a place for the “goto” to jump.
repeat♦ - Repeats the statements between the repeat and end lines, n number or times, or forever.
while♦ - Executes the statements between the “while” and “end” lines while the condition is true.

♦ Used in IntuScope.

See Chapter 3 for an overview of Simulation Templates.

Parameter Manipulation

getparam - Returns the value of a param identified by vec.
getparval - Check .PAR file and returns value if found.
nextparam - Enumerates parameters that have tolerances
nextvector - Returns an alias for the next vector, null if none or the first vector.
null - A special vector that can be used in an expression without being declared.
param - A special vector used to identify an instance or model parameter.
tolerance - Returns the tolerance of a parameter.

Inter-Process Communication (IPC) Commands

The following commands are used for inter-process communication.

errorstop - Halts a remote script on errors and send the error message to the designated process.
setquery - Redirects the output from this script to the named program.
switch - Redirects the output from this script to the named program.

Cursor Control Commands

The following commands are used for cursor control.

homecursors♦ - Sets a cursor 0 to the beginning and cursor 1, and to the end of data.
movecursorleft♦ - Moves cursor to the left of value for named vector.
movecursorright♦ - Moves cursor to the right of value for named vector.
setcursor♦ - Sets a cursor, identified by cursor number, to a value.
setnthtrigger♦ - Same as setTrigger, but repeat num times.
settrigger♦ - Advances the cursor to time when vector goes through value +- change with specified slope.

♦ Used in IntuScope.

Print Commands

The following commands are used for print communication.

print♦	- Prints vectors in a SPICE 2 style output.
printcursors♦	- Prints all cursor values.
printevent	- Prints digital events for a digital node.
printname♦	- Selects next parameter with tolerance, if null gets first one with tol.
printplot	- Prints plot name for which the vector belongs.
printstatus♦	- Prints simulation status to stdErr and status window.
printtext♦	- Prints text strings in columns.
printtol	- Prints the parameter tolerance value.
printval♦	- Prints vector data.
printvector♦	- Prints un-interpolated values for a saved vector.

Simulation Templates & Directives

A Simulation Template is an ICL script that has embedded instructions telling the netlist builder in the schematic capture tool where to insert design specific information. It is used to expand SPICE beyond the traditional limitations of the basic AC, DC, and Transient analyses by allowing parameter variations and multiple analysis passes to be run under one analysis umbrella. The following directives are available to be used in Simulation Template files (*.SCP) along with all ICL commands. Please see the on-line help for complete information and details on Simulation Templates.

#include	- Inserts the named file into the script stream.
#mprint	- Generates “print” commands for user-defined measurements from the saved vectors.
#noprint	- Eliminates the “print” statements generated by SpiceNet in order to minimize the amount of memory required during multiple analysis passes.
#nosave	- Eliminates the save commands generated by SpiceNet in order to minimize the amount of memory required during multiple analysis passes.
#simulation	- Generates the simulation control statements. (Tran, AC, DC, etc.)

♦ Used in IntuScope.

#tolerance - Makes a netlist with tolerances taken from SpiceNet.
#vector - Generates save commands from the user-defined measurement vector list.

IntuScope Commands

The following commands are used exclusively in IntuScope.

askvalues - Prompts the user to enter a list of numerical values or expressions that can be evaluated to single or multi-element vectors.
assertvalid - Evaluates all listed vector names to guarantee they represent existing or available vectors.
copytodoc - Copies the specified trace from the current graph document to another graph document.
destroyvec - Deletes the waveform from the current graph.
loadaccumulator - Loads the accumulator with a single-element vector.
linearize - Formats transient vector data onto a linear scale.
makelabel - Positions a cursor at a vectors data value.
messagebox - Display box with script defined message
movelabel - Moves most recent label to (x,y) in 0.1% of window size (lower-left label to upper-left window).
newplot no argument - When a trace is plotted, a new plot, using a default plot name, will be created.
newplot one argument - When a trace is plotted, a new plot, using a given plot name, will be created.
plot - Plots the named vector in the active plot.
plotf - Plots the named vector in the active plot and formats the vectors name.
plotref - Plots the named vectors as a reference trace.
printunits - Prints a vector's units in the output window.
rename - Renames the specified vector, which must be in the currently active plot.
setdoc - Makes the specified graph document the active document.
setlabel - Sets the border, transparent, rotated, or justify properties of the last label added.
setlabeltype - Changes the next labels font to plain text from rich text.

setmargins - Sets the top, bottom, left, and right margins of the current document in tenths of an inch.
setsource - Specifies the desired source for new data.
setunits - Sets a vector's units.
setvec - Makes the specified vector the active vector, and its plot the active plot.
setscaletype - Sets the types of the current plot's x- and y-axis scales to linear or logarithmic.
settracecolor - Sets the color of all currently selected traces.
settracestyle - Sets the style of all currently selected traces.
setxlimits - Sets the minimum and maximum x-axis value range for the currently active trace.
setylimits - Sets the minimum and maximum y-axis and x-axis value range for the currently active trace.
update - Updates all traces in the active document.

IntuScope Functions

The following functions are used in IntuScope 5 only.

askvalue - Asks the user to enter a number (real or complex) returned by the function.
derivx or differentiatex - Returns the derivative of a vector with respect to the default scale vector (usually time or frequency).
integratex - Returns the integral of a vector with respect to the default scale vector (usually time or frequency).
isdisplayed - Returns 1 if the argument is the name of a vector that is currently displayed as a trace in IntuScope. Otherwise it's 0.
minscale - Evaluates the minimum scale value of the vector between cursor 0 and cursor 1.
maxscale - Evaluates the maximum scale value of the vector between cursor 0 and cursor 1.

Using ICL Scripts

Simple ICL Scripts
The simplest use of a script is to create an alias for an expression to use with the .PRINT command.

To establish an alias;

- Enter the alias command in the IsSpice4 Simulation Control dialog's Script window.
  alias vout 20 * sqrt(v(8)) * @r1[i]

- Add the alias name in a second line under the alias line.

  view tran vout

- Click the DoScript button to execute the script. The vout waveform will be displayed after the next simulation is run.

- To place the same items in a control block, enter the following statements into the input netlist or type them into the Simulation Setup dialog's User Statement's field in the schematic:
  .control
  alias output 20 * sqrt(v(8)) * @r1[i]
  view tran output
  .endc

When a simulation is run, the control block script will be executed automatically.

To establish a Simulation Breakpoint;

• Place a stop command in the IsSpice4 Simulation Control dialog's Script window.
  stop when v(8) < 10m

- Run a simulation by clicking the Start button.

These steps will produce a breakpoint when v(8) < 10m. Output will be generated up until the breakpoint is reached. It is simple to include breakpoints in the input netlist.

- In the Simulation Setup dialog in the schematic, enter the following statement into the User Statement's field.

  *#stop when v(8) < 10m

When the simulation is run the breakpoint will be in effect. It should be noted that the Stress Alarms feature in ICAP/4 can also monitor circuit status without forcing the simulator to pause.

Running Analyses from the Input Netlist

The next step of complexity is encountered when an analysis must be run from within the control block. In this case, the "dot" analysis control commands must be moved into the control block from the netlist. The only exception is the .PRINT command. Although the ICL print command can be used to store data in the output file, the .PRINT command outside the control block is required to produce vectors that can be read by IntuScope.

The basic steps for creating a control block simulation are:

- Issue a save command to save the desired output vectors
- Issue view commands to set up the real-time display
- Issue stop breakpoint commands
- Issue the analysis control command
- Create new vector formats with the let command
- Use the print command to store the simulation output

For example:

```
.control
save v(8)
view tran v(8)
tran 1n 250n
let test = v(8)^2
.endc
.PRINT TRAN V(8) TEST
```

The control block above performs a simple transient analysis. Although not terribly exciting, it forms the foundation for more complex simulations. Commands in the control block are executed in the order they are listed, and are performed before any dot commands outside of the control block. Therefore, swapping the tran and the let commands will result in an error.

Temperature Simulations

Performing an analysis at three different temperatures requires a progression of simulations. To obtain output that can be viewed in IntuScope, each waveform must have a unique name. This can be set up quite easily with the alias command. Consider the following control block;

Output File Data
Input Netlist

```
.control
save all allcur allpow
view ac v(5)
set temp=-55
alias v55m v(5)
ac dec 10 100k 100meg
print v55m
set temp=55
alias v55 v(5)
ac dec 10 100k 100meg
print v55
set temp=125
alias v125 v(5)
ac dec 10 100k 100meg
print v125
.endc
*.PRINT AC V55M V55 V125
```

- The first command encountered within the control block is the save command. This line saves all voltages, currents, and device power dissipations. The save command must be present once the analysis is moved into the control block so that output vectors are created for the desired output variables.

- The next command is the “view” command. Since the analysis has been moved into the control block, the real time display (typically resulting from the .PRINT) will not occur. Hence, the view command is issued.

- Next, the set command is used to set the .OPTIONS parameter TEMP (global circuit temperature). As with the previous two commands, once the analysis is moved inside the control block, the options must be altered with the set command.

- At this point, the analysis is performed. Notice that the syntax is identical to the standard .AC command.

- An alias is then established for the node voltage v(5). This alias produces a unique header for the data at each temperature.

- A print statement produces tabular output for the temperature run by printing the alias.

- To create a curve family in IntuScope, the previous two steps can be replaced with the ICL sendplot command.

From here, the syntax is repeated for each temperature.

- Finally, a .PRINT line is placed outside the control block for compatibility with the IntuScope Waveforms menu for the tabulated data. The .PRINT line is commented out with an asterisk to stop the data from being redundantly stored in the output file. If a curve family is created, then the ∗.PRINT statement is not needed.

Multiple Analyses and Breakpoints

The most straightforward implementation of a breakpoint was discussed earlier. When an analysis control statement is added, the simulation becomes more robust. This is because the simulation is not terminated at the breakpoint. It is merely paused until another command restarts the simulation, or the simulation is aborted. In the following script, the simple simulation and breakpoint are combined.

```
stop when @r1[i] > 10m
tran 1n 250n
print all
delete all
stop when @r1[i] > 15m
resume
```

The delete command removes the breakpoint established by the stop command and allows the simulation to continue.

Simulation Loop
In the following script, a loop is generated in which a resistor value is swept, and a diode's mean power dissipation is monitored. The control block is established with the repeat command and will execute the loop commands 10 times, or until the break command is encountered.

```
save all allcur allpow
view tran @d3[p]
repeat 10
tran 1n 150n
if mean(@d3[p]) > 15m
alter @r17[resistance]=@r17[resistance]+50
print mean(@d3[p])
else
print @r17[resistance] mean(@d3[p])
break
end if
end repeat
```

The 10 parameter on the repeat line could have been removed. However, by limiting the number of times the loop is performed, a safety net is established allowing the simulation to terminate within a reasonable time. A while or dowhile loop would produce similar results using the condition in the If statement.

Note that the if, while, and dowhile loops will only check the power dissipation after the analysis is complete. Hence, the need to reduce the power dissipation vector to a scalar quantity with the mean function. Other functions such as RMS and standard

deviation can be defined using the mean function (see the ICL function command in the Vector section). To check the instantaneous power dissipation during the simulation, a stop breakpoint command is required.

Calculating Harmonics

The circuit contains two sin sources that are multiplied together with a B element. The script sets up several variables and then moves imaginary cursors into position in order to record the proper mean values of the waveforms. (The mean function is one of several cursor relative functions outlined previously in this chapter.) The rest of the script calculates and prints the frequency and associated harmonic.

```
* How to calculate Harmonic components with ICL
v1 1 0 1 sin 0 1 1K
r1 1 0 1
v2 2 0 1 sin 0 1 2K
r2 2 0 1
b2 5 0 v = v(1)*v(2)
r3 5 0 1
.control
view tran V(5)
tran 1u 2m 0 1u          ; do transient analysis
mintime = 0.1u             ; minimum window edge
maxtime = 2m             ; maximum window edge
frequency = 1K           ; base frequency
maxfreq = 6K             ; max frequency of interest
delta = 1K               ; frequency increment
dowhile (frequency < maxfreq)    ; go through all frequency values
setcursor(0, mintime)       ; move cursor 0 to the min window edge
setcursor(1, maxtime)         ; move cursor 1 to the max window edge
vsin = v(5)*sin(2*180*frequency*TIME)
Vcos = v(5)*cos(2*180*frequency*TIME)
vsinmean = mean(vsin)       ; calculate harmonic
vcosmean = mean(vcos)
harmonic = sqrt(vsinmean*vsinmean+vcosmean*vcosmean)
print frequency
print harmonic          ; print results
frequency = frequency + delta     ; increment frequency
end
.endc
.PRINT TRAN V(1) V(2) V(5)
.END
```

Appendices

Appendix A: Solving SPICE Convergence Problems

See the Convergence Wizard for more help with solving convergence problems.

The following techniques on solving convergence problems are taken from various sources including:

[1] Meares, L.G., Hymowitz C.E. "Simulating With Spice", Intusoft, 1988

[2] Muller, K.H. "A SPICE Cookbook", Intusoft, 1990

[3] Meares, L.G., Hymowitz C.E. "Spice Applications Handbook", Intusoft, 1990

[4] *Intusoft Newsletters*, various dates from 1986 to present

[5] The Designer's Guide to SPIC and Spectre, Kenneth S. Kundert, Kluwer Academic Publishers, 1995

[6] The SPICE Book, Andrei Vladimirescu, John Wiley & Sons Inc,, 1994

[7] Inside SPICE, Ron Kielkowski, McGraw-Hill, Inc. 1994

What is Convergence? (or in my case, Non-Convergence)

The answer to a nonlinear problem, such as those in the SPICE DC and Transient analyses, is found via an iterative solution. For example, IsSpice4 makes an initial guess at the circuit's node voltages and then, using the circuit conductances, calculates the mesh currents. The currents are then used to recalculate the node voltages, and the cycle begins again. This continues until all of the node voltages settle to values that are within specific tolerance limits. These limits can be altered using various .Options parameters such as Reltol, Vntol, and Abstol.

If the node voltages do not settle down within a certain number of iterations, the DC analysis will issue an error message such as *"No convergence in DC analysis"*, *"Singular Matrix"*, or *"Gmin/Source Stepping Failed"*. SPICE will then terminate the run because both the AC and transient analyses require an initial stable operating point in order to proceed. During the transient analysis, this iterative process is repeated for each individual time step. If the node voltages do not settle down, the time step is reduced and SPICE tries again to determine the node voltages. If the time step is reduced beyond a specific fraction of the total analysis time, the transient analysis will issue the error message, *"Time step too small,"* and the analysis will be halted.

Problems come in all shapes, sizes, and disguises, but convergence problems are usually related to one of the following:

- **Circuit Topology**
- **Device Modeling**
- **Simulator Setup**

The DC analysis may fail to converge because of incorrect initial voltage estimates, model discontinuities, unstable/bistable operation, or unrealistic circuit impedances. Transient analysis failures are usually due to model discontinuities or unrealistic circuit, source, or parasitic modeling. In general, you will have problems if the impedances, or impedance changes, do not remain reasonable. Convergence problems will result if the impedances in your circuit are too high or too low.

The various solutions to convergence problems fall under one of two types. Some are simply band-aids, which merely attempt to fix the symptom by adjusting the simulator options. Other solutions actually affect the true cause of the convergence problems.

The following techniques can be used to resolve 90 to 95% of all convergence problems. When a convergence problem is encountered, you should start with the first suggestion and proceed with the subsequent suggestions until convergence is

achieved. The suggestions are structured so that they can be incrementally added to the simulation. The sequence is also defined so that the initial suggestions will be of the most benefit. Note that suggestions that involve simulation options may simply mask the underlying circuit instabilities. Invariably, you will find that once the circuit is properly modeled, many of the “options” fixes will no longer be required!

General Discussion

Many power electronics convergence problems can be solved with two option parameters, Gmin and Rshunt. The Gmin option is available in all SPICE 2 and 3 programs. Gmin is the minimum conductance across all semiconductor junctions. The conductance is used to keep the matrix well conditioned. Its default value is 1E-12mhos. Setting Gmin to a value between 1n and 10n will often solve convergence problems. Setting Gmin to a value that is greater than 10n may cause convergence problems.

The Rshunt option causes IsSpice4 to insert a resistor from every node in the circuit to ground. Rshunt is available only in programs such as IsSpice4 that have incorporated the XSPICE enhancements [36]. Setting Rshunt to a value between 100MEG and 1G will typically help. Setting Rshunt to a value of 100K may cause convergence problems.

SPICE does not always converge when relaxed tolerances are used. One of the most common problems is the incorrect use of the ".Options" parameters. For example, setting the tolerance option (Reltol) to a value that is greater than .01 will often cause convergence problems.

The default numerical integration method is the Trapezoidal method. Some circuits will converge better during the transient analysis when the Gear integration method is used. You can invoke Gear integration by adding the statement, .OPTIONS METHOD=GEAR. The Gear method works well for most power electronics simulations.

Setting the value of Abstol to 1u will help in the case of circuits that have currents that are larger than several amps. Again, do not overdo this option. Setting Abstol to a value that is greater than 1u will cause more convergence problems than it will solve.

After you've performed a number of simulations, you will discover the options that work best for your circuits. You can save the .Options line in a text file and use the ".INC filename" command to import the text file. This will allow you to save several .Options lines in text files and explore the use of different sets of options.

If all else fails, you can almost always get a circuit to simulate in a transient simulation if you begin with a zero voltage/zero current state. This makes sense if you consider the fact that the simulation always starts with the assumption that all voltages and currents are zero. The simulator can almost always track the nodes from a zero condition. Running the simulation will often help uncover the cause of the convergence failure.

The above recommendation is only true if your circuit is constructed properly and the netlist is syntactically correct. Most of the time, minor mistakes are the cause of convergence problems. Error messages will help you track down the problems, however, a good technique is to visually scan each line of the netlist and look for anomalies. It may be tedious, but it's a proven way to weed out mistakes.

Not all convergence failures are a result of the SPICE software! Convergence failures may identify many circuit problems. Check your circuits carefully, and don't be too quick to blame the software.

If you've tried everything you can think of, and you still can't get your circuit to converge, you may contact Intusoft's Technical Support staff at info@intusoft.com We can also be reached on the Internet at http://www.intusoft.com.

IsSpice4 - New Convergence Algorithms

In addition to automatically invoking the traditional source stepping algorithm, IsSpice4 contains a superior algorithm called “Gmin Stepping”. This algorithm uses a constant minimal junction conductance, which keeps the sparse matrix well conditioned, and a separate variable conductance to ground at each node, which serves as a DC convergence aid. The variable conductances cause the solution to converge more quickly. They are then reduced, and the solution is recomputed. The solution is eventually found with a sufficiently small conductance. Then the conductance is removed entirely in order to obtain a final solution. This technique has proven to work very well, and IsSpice4 selects it automatically when convergence problems occur. The suggestion (made in a number of textbooks) of increasing the .Options Gmin value in order to solve DC and operating point convergence problems is performed automatically by this new algorithm. Gmin may still be increased (relaxed) for the entire simulation by setting the .Options Gmin value, but this should only be done as a last resort.

Non-Convergence Error Messages/Indications

The following is a list of the key error messages that indicate that convergence has not occurred. In most cases, SPICE 3 will also indicate the element or node that is the source of the failure. This is a feature that is not found in most other SPICE 2 simulators.

- DC Analysis (which includes the .OP analysis and the small signal bias solution that is performed prior to the AC analysis, or Initial transient solution that is calculated prior to the Transient analysis) - *“No Convergence in DC analysis”*, or *“PIVTOL Error”*. SPICE 3 programs such as IsSpice4 issue a *“Gmin/Source Stepping Failed”* or *“Singular Matrix”* message.

- DC Sweep Analysis (.DC) - *"No Convergence in DC analysis at Step = xxx."*
- Transient Analysis (.TRAN) - *"Internal timestep too small."*

Convergence Solutions

Important Note: The suggestions below are applicable to most SPICE programs, especially if they are Berkeley SPICE 3 compatible. If several .Options parameters are used, you can put them on the same line and separate them with spaces.

DC Convergence Solutions

See the Convergence Wizard for more help with solving convergence problems.

1. Check the circuit topology and connectivity.
".Options LIST" will provide a nice summary printout of the nodal connections. It produces a flattened netlist of the entire circuit in the output file. If you are using the SpiceNet schematic entry program, you should perform a "ReNet" to insure that unique node numbers and reference designations are being used and that all circuit elements are properly connected.

Common mistakes and problems:

- Make sure that all of the circuit connections are valid. Check for incorrect node numbering or dangling nodes. Also, verify component polarity.
- Make sure you didn't use the letter O instead of a zero (0).
- Check for syntax mistakes. Make sure that you used the correct SPICE units (i.e., MEG instead of M(milli) for 1E6).
- Make sure that there's a DC path from every node to ground.
- Make sure that there are at least two connections at every node.
- Make sure that there are no loops of inductors or voltage sources.
- Make sure that there are no series capacitors or current sources.

- Place the ground (node 0) somewhere in the circuit. Be careful when you use floating grounds; you may need to connect a large resistor from the floating node to ground.
- Make sure that voltage/current generators use realistic values, and verify that the syntax is correct.
- Make sure that dependent source gains are correct, and that B element expressions are reasonable. If you are using division in an expression, verify that division by zero cannot occur.
- Make sure that there are no unrealistic model parameters; especially if you have manually entered the model into the netlist.
- Make sure that all resistors have a value. In SPICE 3, resistors without values are given a default value of 1 kOhm.
- Negative capacitor and inductor values are allowed in SPICE 3. They will not be flagged as an error, but can cause timestep problems, depending on the topology of the circuit.

2. AUTOTOL, A New IsSpice4 Convergence Aid

There are certain cases for which DC convergence fails because of singularities in the DC operating point. A zero order hold is an example that at DC cascade a Z transform differentiator with a Laplace integrator. The resultant product of 0 times infinity produces a non-convergent DC result; however, an AC crossover network eliminates the problem node so that it is fair to remove it from the convergence test. Increasing VNTOL can remove the non-convergent behavior; however, vntol is global and increasing it to solve the problem at one node will reduce the DC operating point accuracy. If the user were to manually enter VNTOL for each, the bookkeeping management would become difficult. What Intusoft has done is to introduce a new IsSpice4 option, AUTOTOL. An array of values holding vntol[] and abstol[] for each node and source current is initialized with the VNTOL and ABSTOL values. If AUTOTOL is set larger than 1, then when a node or branch current fails to converge, its tolerance value is multiplied by AUTOTOL. Setting AUTOTOL=2 will rapidly eliminate offending nodes. Smaller values will make

the elimination occur more slowly and have a less sever affect. If AUTOTOL is set to less than -1, the same thing occurs using the absolute value of AUTOTOL. The ".OUT" file reports the activity so that you can isolate problem nodes and sources. AUTOTOL is only active for the initial DC operating point calculation.

3. Increase ITL1 to 400 in the .OPTIONS statement.

Example: .OPTIONS ITL1=400

This increases the number of DC iterations that IsSpice4 will perform before it gives up. In all but the most complex circuits, further increases in ITL1 won't typically aid convergence.

4. Set ITL6 =100 in the .OPTIONS statement. (ITL6 is only used for SPICE 2 based simulators). Srcsteps is used for SPICE 3 simulators.

Example: .OPTIONS SRCSTEPS=100

This invokes the source stepping algorithm. The value is the number of steps. **This step is unnecessary for IsSpice4 users,** since source stepping is automatically invoked after both the default method and the Gmin stepping algorithms have been attempted. Note for SPICE 2 users: this is an undocumented Berkeley SPICE 2G option.

Source stepping sets all of the stimulus functions (voltage sources, etc.) to a near zero value in the hopes of easing the calculation of the operating point solution. When a solution is found, the stimulus sources are increased toward their final DC values, and another operating point is calculated using the previous solution as a "seed". This process continues until the sources are at the full DC values and an operating point in produced.

5. Add .NODESETs

Example: .NODESET V(6)=0

View the node voltage/branch current table in the output file. SPICE 3 produces one even if the circuit does not converge. Add .NODESET values for the top level circuit nodes (not the subcircuit nodes) that have unrealistic values. You do not need to nodeset every node. Use a .NODESET value of 0V if you do not have a better estimation of the proper DC voltage. Caution is warranted, however, for an inaccurate Nodeset value may cause undesirable results.

6. Add resistors and use the OFF keyword.

Example: D1 1 2 DMOD OFF
RD1 1 2 100MEG

Add resistors across diodes in order to simulate leakage. Add resistors across MOSFET drain-to-source connections to simulate realistic channel impedances. This will make the impedances reasonable so that they will be neither too high nor too low. Add ohmic resistances (RC, RB, RE) to transistors. Use the .Options statement to Reduce Gmin by an order of magnitude.

Next, you can also add the OFF keyword to semiconductors (especially diodes) that may be causing convergence problems. The OFF keyword tells IsSpice4 to first solve the operating point with the device turned off. Then the device is turned on, and the previous operating point is used as a starting condition for the final operating point calculation.

7.Use PULSE statements to turn on DC power supplies

Example: VCC 1 0 15 DC
becomes VCC 1 0 PULSE 0 15

This allows the user to selectively turn on specific power supplies. This is sometimes known as the "Pseudo-Transient" start-up method. Use a reasonable rise time in the PULSE statement to simulate realistic turn on. For example,

V1 1 0 PULSE 0 5 0 1U

will provide a 5 volt supply with a turn on time of 1 μs. The first value after the 5 (in this case, 0) is the turn-on delay, which can be used to allow the circuit to stabilize before the power supply is applied.

8. Set RSHUNT=xxx in the .OPTIONS statement.

Example: .OPTIONS RSHUNT=100MEG

The Rshunt option places a resistor, of the specified value, from every node in the circuit to ground. Note: if this works, you have indeed changed the operation of the circuit, so make sure that you verify the results carefully.

9. Add UIC (Use Initial Conditions) to the .TRAN statement.

Example: .TRAN .1N 100N UIC

Insert the UIC keyword in the .TRAN statement. Use Initial Conditions (UIC) will cause SPICE to completely bypass the bias point calculation. You should add any applicable .IC and IC= initial conditions statements to assist in the initial stages of the transient analysis. Be careful when you set initial conditions, for a poor setting may cause convergence difficulties.

AC Analysis Note: Solutions 7 through 9 should be used only as a last resort, because they will not produce a valid DC operating point for the circuit (all supplies may not be turned On and circuit may not be properly biased). Therefore, you cannot use solutions 7-9 if you want to perform an AC analysis, because the AC analysis must be proceeded by a valid operating point solution. However, if your goal is to proceed to the transient analysis, then solutions 7-9 may help you and may possibly uncover the hidden problems that plague the DC analysis.

DC Sweep Convergence Solutions

1. Check circuit topology and connectivity.
This item is the same as item 1 in the DC analysis.

2. Set ITL2=100 in the .OPTIONS statement.
Example: .OPTIONS ITL2=100
This increases the number of DC iterations that SPICE will attempt before it gives up.

3. Increase or decrease the step values that are used in the .DC sweep.
Example: .DC VCC 0 1 .1
becomes .DC VCC 0 1 .01
Discontinuities in the SPICE models can cause convergence problems. The use of larger steps may help to bypass the discontinuities, while the use of smaller steps may help IsSpice4 find the intermediate answers that will be used to find the point that doesn't converge.

4. Do not use the DC sweep analysis.

```
Example:    .DC VCC  0  5  .1
            VCC  1  0
becomes     .TRAN .01  1
            VCC  1  0  PULSE  0  5  0  1
```

In many cases, it is preferable to use the transient analysis to ramp the appropriate voltage and/or current sources. The transient analysis tends to be more robust, and is sometimes faster.

Transient Convergence Solutions

1. Check circuit topology and connectivity.
This item is the same as item 1 in the DC analysis.

2. Set RELTOL=.01 in the .OPTIONS statement.
Example: .OPTIONS RELTOL=.01
This option is encouraged for most simulations, since the reduction of Reltol can increase the simulation speed by 10 to

50%. Only a minor loss in accuracy usually results. A useful recommendation is to set Reltol to .01 for initial simulations, and then reset it to its default value of .001 when you have the simulation running the way you like it and a more accurate answer is required. Setting Reltol to a value less than .001 is generally not required.

3. Reduce the accuracy of ABSTOL/VNTOL if current/ voltage levels allow it.

Example: . OPTION ABSTOL=1N VNTOL=1M

Abstol and Vntol should be set to about 8 orders of magnitude below the level of the maximum voltage and current. The default values are Abstol=1pA and Vntol=1μV. These values are generally associated with IC designs.

4. Set ITL4=500 in the .OPTIONS statement.

Example: .OPTIONS ITL4=500

This increases the number of transient iterations that SPICE will attempt at each time point before it gives up. Values that are greater than 500 won't usually bring convergence.

5. Realistically Model Your Circuit; add parasitics, especially stray/junction capacitance.

The idea here is to smooth any strong nonlinearities or discontinuities. This may be accomplished via the addition of capacitance to various nodes and verifying that all semiconductor junctions have capacitance. Other tips include:

- Use RC snubbers around diodes.
- Add Capacitance for all semiconductor junctions (3pF for diodes, 5pF for BJTs if no specific value is known).
- Add realistic circuit and element parasitics.
- Watch the Real-time display (If you have IsSpice4) and look for waveforms that transition vertically (up or down) at the point during where the analysis halts. These are the key nodes that you should examine for problems.
- If the .Model definition for the part doesn't reflect the behavior of the device, use a subcircuit representation. This is especially important for RF and power devices such as RF BJTs and power MOSFETs. Many vendors cheat

and try to "force fit" the SPICE .MODEL statement in order to represent a device's behavior. This is a sure sign that the vendor has skimped on quality in favor of quantity. Primitive .MODEL statements CAN NOT be used to model most devices above 200MEGHz because of the effect of package parasitics. And .MODEL statements CAN NOT be used to model most power devices because of their extreme nonlinear behavior. In particular, if your vendor uses a .MODEL statement to model a power MOSFET, throw away the model. It's almost certainly useless for transient analysis.

6. Reduce the rise/fall times of the PULSE sources.

Example: VCC 1 0 PULSE 0 1 0 0 0
becomes VCC 1 0 PULSE 0 1 0 1U 1U

Again, we are trying to smooth strong nonlinearities. The pulse times should be realistic, not ideal. If no rise or fall time values are given, or if 0 is specified, the rise and fall times will be set to the TSTEP value in the .TRAN statement.

7. Use the .OPTIONS RAMPTIME=xxx statement to ramp up all of the sources.

Example: .OPTIONS RAMPTIME=10NS

Ramptime causes all the independent sources to be ramped up from zero to their initial values at the beginning of the transient analysis. The time is specified by the user. This may be quite helpful if you're having trouble getting the transient analysis to start. Remember to give enough time for the sources to ramp up. If a ramp time is too short, it may cause disturbances that require a long time to settle, or may even cause further convergence problems.

8. Add UIC (Use Initial Conditions) to the .TRAN line.

Example: .TRAN .1N 100N UIC

If you are having trouble getting the transient analysis to start because the DC operating point can't be calculated, insert the UIC keyword in the .TRAN statement. UIC will cause SPICE to completely bypass the DC analysis. You should add any applicable .IC and IC= initial conditions statements to assist in

the initial stages of the transient analysis. Be careful when you set initial conditions, for a poor setting may cause convergence difficulties. (See the Altinit and Ramptime options for more help with UIC cases).

9. Change the integration method to Gear (See also Special Cases below).

Example: .OPTIONS METHOD=GEAR

This option causes SPICE 3 to use Gear integration to solve the transient equations, as opposed to the default method of trapezoidal integration. The use of the Gear integration method should be coupled with a reduction in the Reltol value. This will produce answers that approach a more stable numerical solution. Trapezoidal integration tends to produce a less stable solution that can produce spurious oscillations. Gear integration often produces superior results for power circuitry simulations, due to the fact that high frequency ringing and long simulation periods are often encountered.

Gear integration is very valuable, especially for Power Supply designers. It is included in all IsSpice4 versions. Many popular versions of SPICE, including Pspice™, Hspice™ and Electronics Workbench™ do NOT let you set this valuable and important option.

10. Use the VSECTOL argument to enable the largest error in volts-seconds possible between time steps.

Example: .OPTIONS VSECTOL=50NS

VSECTOL reduces the time step if the product of the absolute value of the error in predicted voltage and the time step exceeds the VSECTOL specification. Using VSECTOL to control the time step produces higher accuracy during the turn-off transition and uses less computational resources when there is no switching activity.

Modeling Tips

Device modeling is one of the hardest steps encountered in the circuit simulation process. It requires not only an understanding of the device's physical and electrical properties, but also a detailed knowledge of the particular circuit application. Nevertheless, the problems of device modeling are not insurmountable. A good first-cut model can be obtained from data sheet information and quick calculations, so the designer can have an accurate device model for a wide range of applications.

Data sheet information is generally very conservative, yet it provides a good first-cut of a device model. In order to obtain the best results for circuit modeling, follow the rule: "Use the simplest model possible". In general, the SPICE component models have default values that produce reasonable first order results. Here are some helpful tips:

- Don't make your models any more complicated than they need to be. Overcomplicating a model will only cause it to run more slowly, and will increase the likelihood of an error.
- Remember: modeling is a compromise.
- Don't be afraid to test your models, especially the ones you did not create.
- Create subcircuits that can be run and debugged independently. Simulation is just like being at the bench. If the simulation of the entire circuit fails, you should break it apart and use simple test circuits to verify the operation of each component or section.
- Document the models as you create them. If you don't use a model often, you might forget how to use it.
- Be careful when you use models that have been produced by hardware vendors. Many have syntactical errors, and certainly DO NOT fully reflect the characteristics of the real part. Check the documentation for a list of characteristics that are supported by the model.

- Semiconductor models should always include junction capacitance and the transit time (AC charge storage) parameters.
- If the .Model definition for a large geometry device doesn't reflect the behavior of the device, use a subcircuit representation.
- Be careful when using behavioral models for power devices. Many SPICE vendors try to pass off power semiconductor models using behavioral modeling techniques. Most SPICE vendors do not have the expertise to create sophisticated subcircuit representations. Behavioral models have their place, but in the case of power devices, they will usually NOT exhibit many important second order effects.

- **And lastly, there is no substitute for knowing what you're doing!!**

Intusoft makes available an inexpensive modeling program. The program, called SpiceMod, is an easy-to-use utility that makes semiconductor models (Diode, Zener Diode, BJT, Power BJT, Darlington BJT, MOSFET, Power MOSFET, JFET, Triac, IGBT, SCR) from data sheet parameters. The models work with ANY SPICE simulator. It has two distinct advantages:

1) It allows you to make a SPICE model based on your design specifications. For example, you can make a model for 1A 100V diode. You can then simulate your circuit and refine the boundaries for the type of part required. You can assign the actual part number at a later time. This eliminates the need for your SPICE vendor to supply models for every possible part number.

2) Models are created from data sheet values. If you do not have all of the parameters, SpiceMod will estimate the data you do not have, based on the data you do have. Therefore, it never leaves key SPICE parameters (capacitance, transit time, etc.) at their default values. The use of these default values is the simplest way to make a good model useless.

SpiceMod is highly recommended.

Repetitive And Switching Simulations

Switching simulations refer to simulations that have a significant number of repetitive cycles, such as those found in SMPS simulations. Simulations such as these can experience a large number of rejected timepoints. Rejected timepoints are due to the fact that SPICE has a dynamically varying timestep, which is controlled by constant tolerance values (Reltol, Abstol, Vntol). An event that occurs during each cycle, such as the switching of a power semiconductor, can trigger a reduction in the timestep value. This is caused by the fact that SPICE attempts to maintain a specific accuracy, and adjusts the timestep in order to accomplish this task. The timestep is increased after the event, until the next cycle, when it is again reduced. This timestep hysteresis can cause an excessive number of unnecessary calculations. To correct this problem, we can regress to a SPICE version 1 methodology and force the simulator to have a fixed timestep value.

To force the timestep to be a fixed value, set the Trtol value to 100, i.e., .OPTIONS TRTOL=100. The default value is 7. The Trtol parameter controls how far ahead in time SPICE tries to jump. The value of 100 causes SPICE to try to jump far ahead. Then set the Tmax value in the .TRAN statement to a value that is between 1/10 and 1/100 of the switching cycle period (.TRAN tStep tStop tStart TMAX). This has the opposite effect; it forces the timestep to be limited. Together, they effectively lock the simulator timestep to a value that is between 1/10 and 1/100 of the switching cycle period, and eliminate virtually all of the rejected timepoints. These settings can result in over a 100% increase in speed!

Note: In order to verify the number of accepted and rejected timepoints, you may issue the .OPTIONS ACCT parameter and view the data at the end of the output file.

Other Convergence Helpers

For those users who are using a version of SPICE based on Berkeley SPICE 3, such as IsSpice4, several other options are also available:

1. Gminsteps (DC Convergence)

Example: .OPTIONS GMINSTEPS=200

The Gminsteps option adjusts the number of Gmin increments that will be used during the DC analysis. **Gmin stepping is invoked automatically when there is a convergence problem.** Gmin stepping is a new algorithm in SPICE 3 that greatly improves DC convergence.

2. ALTINIT function (Transient Convergence with UIC)

Example: . OPTION ALTINIT=10

Setting Altinit to 1 causes an alternate (more lenient) algorithm to be used when the UIC keyword is issued in the .TRAN statement. Normally, this alternate algorithm is automatically invoked when the default method fails. A number other than 1 refers to the initial timestep jump, which will be used to determine the first timepoint. The default value is 1E-20 seconds. It can be varied from 1E-10 to 1E-30 seconds. The value of 1E-10 (i.e., Altinit=10) will reduce the accuracy of the first timepoint, but will make it easier for IsSpice4 to start the transient simulation. The Altinit option is unique to IsSpice4.

Special Cases

Mosfets - Check the connectivity. Connecting two gates together, but to nothing else, will give a PIVTOL/Singular matrix error. Check the model Level parameter. SPICE 2 programs do not behave properly when MOSFETs of different levels are used in the same simulation.

SPICE 3 Convergence Helpers

For those users who are running a version of SPICE based on Berkeley SPICE 3, several other options are also available.

1. Gminsteps (DC Convergence) - Same as ITL6
Example: .OPTIONS GMINSTEPS=200

The Gminsteps option adjusts the number of increments that Gmin will be stepped during the DC analysis. Gmin stepping is invoked automatically when there is a convergence problem. Gmin stepping is a new algorithm in IsSpice4 that greatly improves DC convergence.

2. ALTINIT function (Transient Convergence)
Example:.OPTIONS ALTINIT=1

Setting ALTINIT to one causes the default algorithm used when the UIC (use initial condition) keyword is issued in the .TRAN to be bypassed in favor of a second more lenient algorithm. Normally, the second algorithm is automatically invoked when the default method fails.

Appendix B: Device and Model Parameters

The Device and Model Parameter tables summarize all the input and output parameters available for each of the devices and models in IsSpice4. The tables can be found in the on-line help. Use the Search button to locate the “device parameters” topic or the type of device you are interested in. Help on the device’s parameter list will be available. Both Parameter names and descriptions are stored.

There are up to three different sections for each type of device (Input-only, Input-Output, and Output-only). Some devices will also have a set of model parameters. Input parameters to devices and models are simply parameters that can occur on a device or model definition line in the form of “keyword” (such as the BJT device area parameter) or “keyword=value” (such as BF=100, the BJT beta parameter). These parameters can be set by the ICL alter command. Output parameters are computed measurements that provide information about a device or model. These parameters are specified as “@device[keyword]” and are available for the most recent point computed or, if specified in a .PRINT or ICL save statement, for an entire simulation as a normal output vector. See the .PRINT and ICL alter, save, view, show, showmod and print functions for more information.

Some variables are listed as both input and output, and their output simply returns the value stated in the netlist, or the default value after the simulation has been run. Many such input variables are available as output variables in a different format, such as the initial condition vectors, which can be retrieved as individual initial condition values. Finally, internally derived values are for output only and are provided mainly for transient and operating point output purposes.

Appendix C: IsSpice4 Error and Warning Messages

The following error and warning messages are arranged alphabetically under two headers, Errors and Warnings. A brief explanation accompanies each message.

It should be noted that IsSpice4 does not abort a simulation just because an error is encountered. Instead, an message is placed in an error file and displayed in the Errors window. IsSpice4 tries to complete the simulation unless a serious error is encountered. Frequently, this will allow analyses not affected by the error to run properly. This is different from SPICE 2 programs where any error immediately stopped the simulation.

IsSpice4 will notify you that an error has occurred by blinking a question mark in the simulation status field (upper left corner of the screen). You may choose to abort the simulation or let it continue. The real time waveform displays can be used as an indication of the simulation's validity.

When running from ICAPS, the error file will automatically be opened using the IsEd text editor if an error is detected during simulation.

Errors

Error: .TRAN step time less than or equal to zero

This error will occur when the TSTEP parameter in the .TRAN statement is less than or equal to zero.

Error: length too small to interpolate

This error will occur when there is no raw internal data to interpolate. This can happen if an analysis does not run because of a syntax error in the control statement. For example, the following line, with an incorrect TSTART parameter, will generate this message;

```
.tran 1n 100n 0 100
```

Error: no such subcircuit: <name>

This means that a subcircuit call line appears for a subcircuit that is not defined in the netlist. For instance, if the line "X1 2 3 4 SWT" appears in the netlist, but there is no subcircuit definition (.SUBCKT) for SWT.

Error: no such vector

This error will appear when a .PRINT statement is not included for an analysis type being run. For instance, if an AC analysis was run and there was no .PRINT AC in the circuit netlist this error message would appear. This error can also occur if a .PRINT statement contains a reference to a nonexistent node or voltage source.

Error: realloc

This error will occur when there is not enough contiguous memory left for the IsSpice4 to use. The memory use meter will display all the available memory, not available contiguous memory. Therefore, it is very likely the memory use meter will show memory left even though it may not be able to be used.

Error: unable to find definition of model <name> - default assumed

This error message will appear if there is no .MODEL statement for a model name referenced on a device call line. This will happen if the model, name, was misspelled in either the .MODEL statement or the call line. This can also occur if the wrong number of nodes is given for a device, because IsSpice4 may assume that the model name is a node number or an extra node number is the model name.

For instance, D1 1 3 9 9 DLASER will generate;

Error unable to find definition of model 9 - default assumed.

Note: Since the BJT model has an optional substrate node a misspelled model name may be interpreted as an node name for the substrate node. In this case, the following may occur. The lines;

```
Q1 1 2 3 qn
.MODEL qn1 NPN
```

will generate the error message;

```
unable to find definition for model - default assumed
warning: singular matrix check nodes qn and qn
```

The string “qn” was assumed to be the optional substrate node and the model name was assumed to be missing.

Error: unimplemented control card

This is caused by a misspelled or unknown control statement. For example;

```
.trn 1n 100n
```

Error: unknown model type <name> - ignored

This error is caused by use of an unknown model type name. For a list of the valid model types, see the .MODEL statement syntax. For instance,

```
.MODEL SWT S(RON=1 ROFF=100)
```

would generate the message

```
.MODEL SWT S(RON=1 ROFF=100)
  unknown model type s - ignored
```

This is notifying you that the input file has a reference to a nonexistent model type, “s”. The correct type should have been SW.

Error: unknown device type

This means that the keyletter in the reference designation is unknown. This is commonly caused by a typographical error. For example, the following line was meant to call a lossy transmission line;

```
p1 1 2 3 4 lossy
```

The key letter for the lossy line element is “o” not “p”. Since the keyletter “p” does not represent any device, IsSpice4 issues the error message.

Error: unknown parameter on <name> - ignored

This error message will appear when a misspelled or incorrect parameter is found. The name of the control statement that contains the bad parameter will appear in the error message. For example, the line below;

.tran 1n 100ns ons 10ns

will generate the error message

Error: unknown parameter on .tran - ignored

The “o” (supposed to be a zero) is not a valid entry and was ignored.

Fatal error: DCtrCurv: source <name> not in circuit

This error will appear when the voltage or current source referenced in a .DC statement does not appear in the circuit netlist. The string <name> will be replaced with the voltage source reference designation that can not be found in the circuit netlist.

Fatal error: <name> : lossy line length must be specified

The “len” parameter in the .MODEL statement for a lossy transmission line must be specified. The string <name> will be replaced with the model name of the incorrect transmission line .MODEL statement.

Fatal error: <name> : <combination> line not supported yet

You have constructed a lossy transmission line using a combination of R, L, C, and G that is not supported. <name> is the name of the lossy model and <combination> is the combination that is not supported.

Fatal error: <name> : transmission line z0 must be given

This error message is stating that the transmission line has no characteristic impedance specified. The string <name> will be replaced with the reference designation of the incomplete transmission line.

Error: Scalar port expected, [found

A scalar connection was expected for a particular port on the code model, but the symbol that is used to begin a vector connection list was found.

Error: Unexpected]

A] was found where is was not expected. Most likely caused by a missing [.

Error: Unexpected [- Arrays of arrays not allowed

A [character was found within an array list already begun with another [character.

Error: Tilde not allowed on analog nodes

The tilde character was found on an analog connection. This symbol, which performs state inversion, is only allowed on digital nodes and on User-Defined Nodes only if the node type definition allows it.

Error: Not enough ports

An insufficient number of node connections was supplied on the instance line. Check the Interface Specification File for the model to determine the required connections and their types.

Error: Expected node identifier

A special token (e.g. [ ] < > ...) was found when not expected.

Error: model: <name> - Array parameter expected - No array delimiter found

An array (vector) parameter was expected on the .model card, but enclosing [ ] characters were not found to delimit its values.

Error: model: <name> - Unexpected end of model card

The end of the indicated .model line was reached before all required information was supplied.

Error: model: <name> - Array parameter must have at least one value

An array parameter was encountered that had no values.

Error: model: <name> - Bad boolean value

A bad value was supplied for a Boolean. Value used must be TRUE, FALSE, T, or F.

Code Model Errors

Code Model core: Magnetic Core

limit_error:

CORE:

This message occurs whenever the input_domain value is an absolute value and the H coordinate points are spaced too closely together (overlap of the smoothing regions will occur unless the H values are redefined).

Code Model d_osc: Digital Oscillator

d_osc_negative_freq_error:

D_OSC: The extrapolated value for frequency has been found to be negative... Lower frequency level has been clamped to 0.0 Hz.

Occurs whenever a control voltage is input to a model that would ordinarily (given the specified control/freq coordinate points) cause that model to attempt to generate an output oscillating at zero frequency. In this case, the output will be clamped to some DC value until the control voltage returns to more reasonable value.

Code Model d_source: Digital Source

loading_error:

D_SOURCE: source.txt file was not read successfully.

This message occurs whenever the d_source model has experienced any difficulty in loading the source.txt (or user-specified) file. This will occur with any of the following problems:

- Width of a vector line of the source file is incorrect.
- A timepoint value is duplicated or is otherwise not monotonically increasing.
- One of the output values was not a valid 12-state value (0s, 1s, Us, 0r, 1r, Ur, 0z, 1z, Uz, 0u,1u, Uu).

Code Model d_state: State Machine

loading_error:

D_STATE: state.in file was not read successfully. The most common cause of this problem is a trailing blank line in the state.in file

This error occurs when the state.in file (or user-named state machine input file) has not been read successfully. This is due to one of the following:

- The counted number of tokens in one of the file's input lines does not equal that required to define either a state header or a continuation line (Note that all comment lines are ignored, so these will never cause the error to occur).
- An output state value was defined using a symbol that was invalid (i.e., it was not one of the following: 0s, 1s, Us, 0r, 1r, Ur, 0z, 1z, Uz, 0u, 1u, Uu).
- An input value was defined using a symbol that was invalid (i.e., it was not one of the following: 0, 1, X, or x).

Code Model d_state: State Machine

index_error:

D_STATE: An error exists in the ordering of states values in the states->state[] array. This is usually caused by noncontiguous state definitions in the state.in file

This error is caused by the different state definitions in the input file being noncontiguous. In general, it will refer to the different states not being defined uniquely, or being "broken up" in some fashion within the state.in file.

Code Model oneshot

oneshot_pw_clamp:

ONESHOT: Extrapolated Pulse-Width Limited to zero

This error indicates that for the current control input, a pulse-width of less than zero is indicated. The model will consequently limit the pulse width to zero until the control input returns to a more reasonable value.

Code Model pwl

limit_error:

PWL:

This error message indicates that the pwl model has an absolute value for its input_domain, and that the x_array coordinates are so close together that the required smoothing regions would overlap. To fix the problem, you can either spread the x_array coordinates out or make the input_domain value smaller.

Code Model s_xfer

num_size_error:

S_XFER: Numerator coefficient array size greater than denominator coefficient array size.

This error message indicates that the order of the numerator polynomial specified is greater than that of the denominator. For the s_xfer model, the orders of numerator and denominator polynomials must be equal, or the order of the denominator polynomial must be greater than that of the numerator.

Code Model sine, square, or triangle

Source_name: Extrapolated frequency limited to 1e-16 Hz

This error occurs whenever the controlling input value is such that the output frequency ordinarily would be set to a negative value. Consequently, the output frequency has been clamped to a near-zero value.

Warnings

Warning: .options card unsupported

This is caused by an obsolete or misspelled parameter in the .OPTIONS statement.

Warning: .TEMP card obsolete - use .options TEMP and TNOM

The .TEMP card supported by SPICE2 simulators is not supported by IsSpice4. The circuit temperature is set using the .OPTIONS TEMP parameter. The temperature at which the model parameters were calculated at, TNOM, is also set in the .OPTIONS statement. See Chapter 10 for the correct syntax.

Warning: <name> : no DC value, transient time 0 used

This message notifies you that the voltage source referenced by the string <name> has no DC voltage value for an initial DC operating point calculation. This is acceptable because IsSpice4 will use the initial transient voltage, or if no transient statement exists, a value of 0, when determining the initial DC operating point.

Warning: can't parse <name> : ignored

This warning is caused by a typographical error in the input circuit netlist. Check the netlist for correct syntax. The string, <name>, will display the character string that was not read into the IsSpice4 program properly.

Warning: device already exists, existing one being used

This is caused by a duplicate reference designation. For example, the existence of two resistor statements beginning with "R1". IsSpice4 will use the only one of the elements. Check the netlist and make sure each reference designation is unique.

Warning: singular matrix: check node <name> and <name2>

This warning can be caused by a node that is not connected to anything. Check the netlist for dangling nodes. The string <name>, and <name2> will be replaced by the node numbers creating the singularity.

Warning: Gmin stepping failed

This warning will occur if a stable DC operating point can not be found. The Gmin stepping algorithm in automatically invoked if the a DC operating point can not be found within ITL1 Newton-Raphson iterations. If Gmin stepping fails, the source stepping algorithm is invoked. This error can also occur if the element connections are not correct. See the warning, “singular matrix:”

Warning: source stepping filed.

This warning message is similar to the one given for Gmin stepping. If a DC operating point can not be found after running the Gmin and source stepping algorithms, IsSpice4 will abort the analysis. At this point you should check the circuit connections for validity and increase the ITL1 value in the .OPTIONS statement before rerunning the simulation.

Warning: time step to small

This warning is caused by the simulator's inability to find a stable answer. Most often this is due to unrealistic circuit modeling or impedances. At this point you should check to see that all of the device models have junction capacitance added, increase the ITL4 value in the .OPTIONS statement, and set RELTOL, also in the .OPTIONS statement, to .01 before rerunning the simulation.

Warning: too few nodes: <name>

This warning is caused by incorrect syntax. Check the input circuit netlist. The string, **<name>**, will contain the character string that has too few nodes. Search for the string in the input netlist and correct any mistakes.

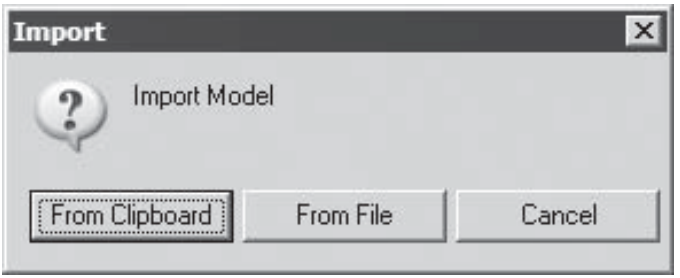
Warning: Singular matrix Trying alternate initialization

Occurs during a solution of initial conditions when using the UIC parameter on the .TRAN line. This error means that inaccurate initial conditions are carrying infinite current. (i.e., parallel capacitors with different initial conditions) The resulting initialization will not be the exact value specified.

Appendix D: Adding a SPICE Model

Importing SPICE model with Library Manager

Adding a SPICE model to ICAP/4's Part Browser is easy using Library Manager. It automatically adds the appropriate *SRC= and *SYM= lines to the Spice model netlist. Start ICAPS and then choose *Import Spice Model…* under the *File* menu. This brings up a dialog that allows you to import spice model netlist from the clipboard or a text file.



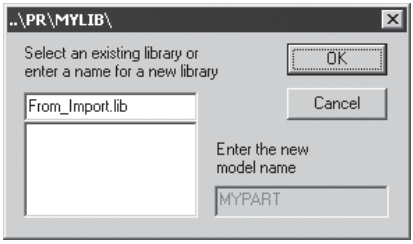
Note: Comment lines start with *. ICAP/4 software uses 5 asterisks as Spice model netlists delimiter.

If the text file contains only one device model, then just import the model "From File." If you have multiple Spice models in the text file, then each model must be imported one at a time. Library Manager will treat any text read-in as a complete model, so only highlight the specific model, copy to clipboard (<Ctrl>+C), and import model "From Clipboard."

- Open up the text file or view webpage with model text.
- Highlight everything from .subckt line to the .ends line of one specific model you want to add, and then copy selected text to the clipboard.
- Press the "From Clipboard" button to import model based only on what is currently stored on the clipboard.

If the model name already exists in your part database, Library Manager will replace your existing model netlist with the text on your clipboard. You will see a text difference between existing and imported spice model netlist. If you don't want the existing model in the part database replaced with your imported model, then exit Library Manager without saving changes, and re-import the model with a modified model name on the .subckt line.

Save New Model

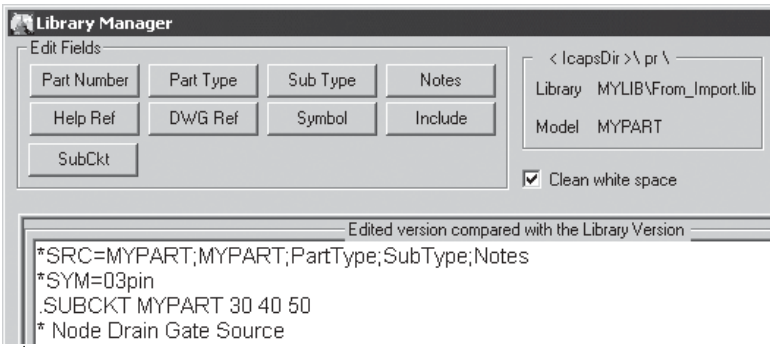


The New Model dialog will only come to view if the model name on the .subckt line does NOT already exist in the part database. The unique model name will be shown in the bottom right field under "Enter the new model name."

Make sure that you save the model to a library file that is NOT included with our installation. If you save to an existing library that Intusoft provides, then it will be overwritten when you install an ICAP/4 product update. All current library files in the part database are shown in the list on the left of the New Model dialog. To save to a new library file, type a unique library name, then press the OK button. You can select an existing library file and keep on adding new models to the same library file. Just make sure that this file is not one of Intusoft's provided library files. An example of a safe library file you could save your models to is "User.lib." This file is not included in the installation and is the default file for imported models.

Define Where to Find Model in Part Browser

Notice that *SRC= and *SYM= have been added to the top of your imported model. These lines link to our Part Browser and symbol.



The *SRC= line contains the information used by SpiceNet's Part Browser for part selection. It will be given the above default text except for where you see MYPART. This text is based on the model name assigned on the .subckt line. 03pin is based on the number of nodes on the .subckt line.

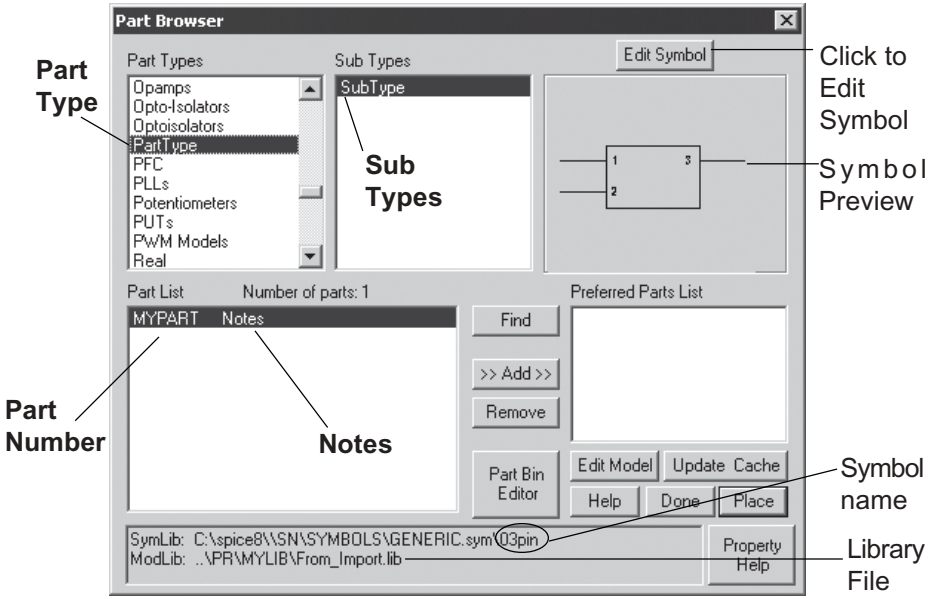
You can modify the text shown in the Part Browser by using the Edit Fields buttons. Each Edit Field is separated by a semicolon. There MUST be four semicolons on the *SRC= line.

*SRC=Part Number;SubCkt;Part Type;Sub Type;Notes

Note: The length of the Part Number and Notes field combined should be no longer than 30 characters. The Part Type and Sub Type each should be no longer than 13 characters. The SubCkt field MUST be unique and match the model name on the .subckt line below. Spaces or !@#$%^&* characters are NOT allowed for the SubCkt field.

After you are done modifying the source line *SRC= and symbol line *SYM=, you MUST save your changes and update the part database.

Validating That Your Part Was Added



Note: SymLib and ModLib at the bottom of the Part Browser dialog reveals the location of the part symbol and netlist.

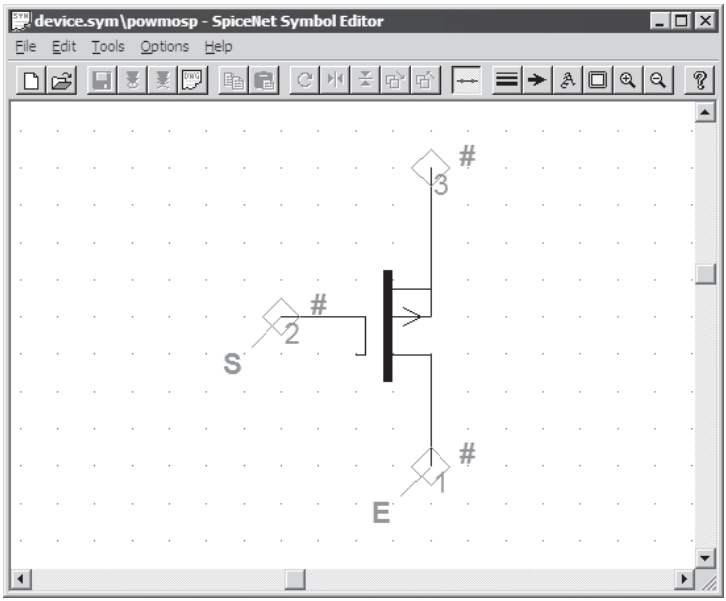
Bring to view your imported model in the part browser to make sure everything is working properly. This step validates that your *SRC= and *SYM= lines were correct.

- Start ICAPS.
- Select *Part Browser* from the *Part* menu or type "x" on the keyboard.
- Click "Find" button and search for your part.

Use Existing Symbol

The symbol name is shown on the SymLib line after the compound symbol file, which ends with .sym extension. If you want to use an existing symbol then select a similar part with the correct pins. Click the "Edit Symbol" button on the Part Browser to open the Symbol Editor and make sure the pin order matches the order of pins on the .subckt line of your added model. If it does, then click “Edit Model” button in the Part Browser to bring up Library Manager. Then, click on the “Symbol” button and type the symbol name.

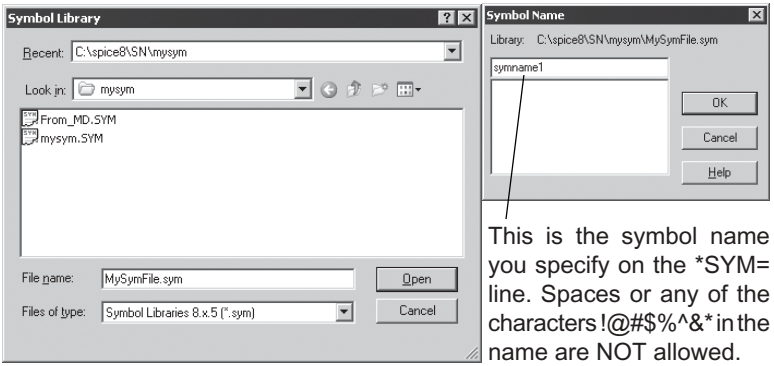
Example: We imported a PNP Power MOSFET model. Notice that in the Parts Browser for existing PNP Power MOSFETs, they use a powmosp symbol in the device.sym compound symbol file. If the edit symbol button is clicked, pin1 is on drain, pin2 is on the gate, and pin3 is on the source. This is the desired symbol, so the symbol name powmosp can be used for the *SYM= line. If the pins didn’t match, one can either reorder the nodes on the subckt line or modify the pins on the symbol.



PIN ORDER #1 #2 #3
.SUBCKT MYPART 30 40 50
* NODES: DRAIN GATE SOURCE

Create New Symbol or Modify Existing Symbol

You can create a new symbol or modify an existing symbol. Just make sure that it is NOT saved in an Intusoft provided compound symbol file. If you do, the file will be overwritten when you update or reinstall the software. Many models link to the same symbol. Remember to check the pin order and number of pins.



This is the symbol name you specify on the *SYM= line. Spaces or any of the characters !@#$%^&* in the name are NOT allowed.

- Choose *Save copy as…* from the *File* menu in Symbol Editor.
- Enter the compound symbol file name you want to save your new symbol to, and press the Open button.
- Now type your symbol name and press OK.

If you saved this symbol to a new compound symbol file, then you need to edit the Sym.@@@ file located in the Spice8\SN directory.

For example, you would add the line **..\sn\mysym\MYSYMFILE.SYM** to the SYM.@@@ file as shown below if your compound symbol file name was MYSYMFILE.SYM. Note: The existing paths are relative but you can specify an absolute path if you want.

```
..\sn
..\sn\symbols
..\sn\symbols\device.SYM
..\sn\symbols\digital.SYM
..\sn\symbols\lin-ic.SYM
..\sn\symbols\special.SYM
..\sn\symbols\system.SYM
..\sn\symbols\ttl74xx.SYM

..\sn\mysym\MYSYMFILE.SYM
```

You can save all your new symbols in one compound symbol file so you don't have to repeat the above step each time.

Create a Folder to Contain Your Own Models

If you want to separate your libraries from the libraries provided by Intusoft, you must modify the LIB.@@@ file located in the Spice8\SN directory.

For example, you would add the line C:\MYLIB to the LIB.@@@ file as shown below, if your model library file was placed in the C:\MYLIB directory. Only .LIB files in the specified directories will be added to the part database.

..\pr
C:\MYLIB

Eliminating Duplicate Parts Errors

To compile the new part database, Start ICAPS, select the *Update Part Database…* from SpiceNet *File* menu, or by selecting MakeDB in ICAP_4 program group. You must resolve all duplicate part errors in the libraries after MakeDB is done compiling.

Compiling User.LIB
-- Warning: Duplicate .MODEL or .SUBCKT name MYPART in POWMOS.LIB

In order to correct this use IsEd to find and modify one of the duplicate subckt part names. If you find a large number of duplicate parts within a single library, you can change the .LIB extension to .LBK so MakeDB will ignore it.

What MakeDB does in more detail

To access parts from the Part Browser dialog, SpiceNet must be able to access two database files, dbase.@@@ and index.@@@. The source files from which these two files are created, and the utility program (MakeDB.exe) used to update the database files, are located in the C:\spice8\sn directory. Editing of the source files and recompilation of the database files is necessary if you want to:

- Add your own IsSpice4 models or subcircuits to SpiceNet to be able to place them with the Part Browser.
- Add a new symbol to represent a new or existing subcircuit.

The files that tell MakeDB.exe which libraries and symbols to compile into the part database are:

- Lib.@@@ This file contains the path(s) to the library directories to be included in the index.@@@ file. All files with a .LIB extension in the directories listed (NOT subdirectories) will be compiled. By default this contains only ..\PR. Relative path is taken to be relative to MakeDB.exe. Explicit path is used as is.
- Sym.@@@ This file contains a list of all of the compound symbol files to be used when compiling the SpiceNet database. The first entry must be "..\SN." Each remaining entry is a compound symbol file. The compound symbol file must have a .SYM extension. Any entry using an implicit path is considered relative to MakeDB.exe. Any entry using an explicit path is used as is.

The following entities are created after compiling the symbol/ library database:

- dbase.@@@ This is a compiled database file made from *SRC lines in the library files. The information in this file is used by SpiceNet's Part Browser dialog and component placement by part number.
- index.@@@ This is a compiled index file containing the name of every model and subcircuit, the library file containing the model/subcircuit, and its corresponding SpiceNet symbol (*SYM).

Appendix E: Export Schematic of Model as Subckt

Make Configuration For Export

Prepare a circuit configuration with only the circuitry that you want to include in the subcircuit. This will most likely require that you remove any test circuitry or stimulus sources. Along this line, be sure to attach wires, test points or continuation symbols on any nodes that are unconnected. In this way, unconnected parts will have their pins resolved with node numbers or names.

Let's cover the basic steps to accomplish this task. We will start with a set of circuitry that is on one layer in one configuration in SpiceNet. We'll then split the circuitry into two parts: one part, which is not needed for the subckt export, will be on a layer called "Test Circuitry." The second, which contains the circuitry destined for subckt export, will be on a second layer called "Circuit Under Test." Then we'll create two configurations called, "For Simulation" and "For Export." The "For Simulation" configuration will contain both layers. The "For Export" configuration will only contain the "Circuit Under Test" layer. Note that items on a layer that is unique to a configuration, will not affect other configurations.

To create a new circuit configuration that uses a portion of your existing circuitry

- Select Options > Layers...
- Click the Rename… button and type "Circuit Under Test." Select OK.
- Click the New… button to create a new layer. Name the new layer "Test Circuitry." Select OK.
- Select OK to close the Layers dialog. All of the circuitry is now on the "Circuit Under Test" layer. We can see this by pressing the eye icon at the bottom left of the schematic windows next to the layers drop-down list. Only parts on the selected layer should be highlighted.
- Select ONLY the circuitry that you do NOT want represented in your exported subckt. Remove all test circuitry and stimulus sources by holding down the <Shift> key, and select each component that you want to exclude.

- Right mouse click and choose Move Item to Layer > “Test Circuitry” to transfer all selected components to the “Test Circuitry” layer.
- Config 1 now has the circuitry split on two layers. We can confirm this by selecting the “Test Circuitry” layer in the drop-down list at the lower left corner of the schematic, and then pressing the eye icon next to the list.
- Select Options > Configuration > Edit…
- Click the Edit… button and rename "Config 1" to "For Simulation.” Select OK.
- Click the New… button and create a new configuration. Call it "For Export.”
- Remove (deselect) the newly created layer ("Test Circuitry") from the configuration. Select OK.
- Select OK again to close the dialog.
- Change between the two configurations by using the toolbar configuration dropdown (left). Notice the differences. The layers available in the dropdown list at the lower left corner of the schematic are based on which layers are in the selected configuration.

Note: In order to account for unconnected parts, whose connections are via parts on layers that are not active in this configuration, you MUST attach a wire, test point or continuation symbol(s) to the unconnected pins. Every pin on every part must have a node number or name. Pins on the ends of dangling wires are OK.

Define Subckt Parameters

If you use parameters text block to define global parameters, then you need to manually copy and paste your parameters to the “For Export” configuration. Global parameters will become your exported subckt parameters. The Parameters text block takes all parameters listed in a schematic text block if it starts with the keyword “parameters,” and moves them to the selected configuration global parameters list when you simulate.

- Select Actions > Simulation Setup > Parameters Setup…
- Copy and paste parameters from “For Simulation” to “For Export” configuration
- Define default parameters or use three question marks (???) if you want user to define passed parameters

Before exporting this configuration, you need to make a subdrawing to define the subckt nodes.

- Select Subdrawings > Make Subdrawing…
- The Subdrawing name is the same name as the current configuration. You may change it in the Subdrawing Name: field.
- Click on the node from the list of nodes on the left, that you want to expose from inside the subcircuit (external connection, and that will be on the .SUBCKT line)
- Click the Add button to add the selected node to the list of subcircuit pins. Repeat this operation for each node you want to expose.
- You may arrange the node order using the Move Up/Move Down buttons. You can also assign the pins to be hidden. You will then be able to make connections to the hidden pins by using a continuation symbol with the same name as the hidden pin. The hidden pin name is assigned inside of the part’s Properties dialog.
- Select your symbol. “Use Wizard to Create Symbol…” enables you to specify pin arrangement and names. "Use Default Symbol" is just a rectangle with the number of pins you expose. If you choose “Get Symbol From Library,” you need to select an existing symbol.

Wizard Note: If you use the Wizard option you MUST save the symbol you make in a compound symbol library file before selecting the Finish Subdrawing button at the bottom of the Symbol Editor screen. This requires you to enter a symbol file name, plus a name for the individual symbol. If the compound symbol file is new, then you must specify the path and symbol file name in SYM.@@@ before you run MakeDB. Remember

the symbol name, and NOT the compound symbol file name. You will need to add this symbol name to the *SYM= line in the subcircuit netlist you generate.

Exporting the Subcircuit Netlist

- Select File > Export…
- Select the SubCkt option from the drop-down list. Select OK.

The subckt part will be added to SPICE8\PR\USER.LIB. Make sure the appended model is not a duplicate model. Modify the *SRC= and *SYM= line so the part is placed in the Part Browser where you desire, and uses the symbol you want. If you have Library Manager, you will be able to specify any library file you desire, and your modifications to the *SRC= and *SYM= line will NOT be overwritten every time you reexport.

Make Your Exported Subckt Model Easier to Use

After you export your subckt model, you will want to add a few modifications to make it easier for other people to use.

- Modify the *SRC= line so you can easily find it in the Part Browser. See Appendix D on how to modify this line.
- Modify the *SYM= line so you are using an easily recognizable symbol. See Appendix D on how to modify this line.
- Add comment lines explaining passed parameters and their units. If a line starts with one asterisk it is considered a comment line. Be careful. Models are separated by a row of at least five asterisks, "*****". If you add rows of asterisks to separate sections of your model, or create a box out of asterisks, then you will be inadvertently cutting your model into pieces.
- Link your subckt model to the schematic you exported it from.. In Library Manager you can press the "DWG Ref" button to browse for your schematic file and add the proper *DWG line. At any time you can bring this up in Library Manager and press the "Test" button to launch your reference schematic. Note: Schematics can't be launched in SpiceNet if the part browser is open.

  The format is: *DWG=Path\Filename

- Create .RTF (Rich Text Format) Help on how to use your subckt model. The Property Help button in the X… Parts Browser dialog, and in each Part Properties dialog, brings up the referenced help. Click on the “Help Ref” button to safely create your own RTF help for your added model.

  The format is: *HELP=pr\<library>\<model>.RTF

- Add *FAMILY line to enable auto-bridging for non-analog pins, or to make hidden pins available. If a subcircuit has no *FAMILY line, SpiceNet will assume that all pins are analog and no bridging will occur. The names used for this line are symbolic names that represent bridging components that will be used when the part is connected in SpiceNet. If a subcircuit that uses a combination of analog and digital connections is constructed, the *FAMILY line is used to make sure that each connection point is properly translated.

  Note: The *FAMILY line is located inside the subcircuit definition (after the .subckt line and before the row of asterisks marking the end of the subcircuit). This is a requirement of the *FAMILY line.

  The following *FAMILY terms are predefined. You can control these levels by selecting Options > Mixed Signal Properties… in SpiceNet.

  "Dout" - generic bridge using TTL levels
  "Din" - generic bridge using TTL levels
  "TTLout" - TTL bridge using TTL levels
  "TTLin" - TTL bridge using TTL levels
  "ECLout" - ECL bridge using ECL levels
  "ECLin" - ECL bridge using ECL levels
  "Rout" - Real bridge using R2A bridge
  "Rin" - Real bridge using A2R bridge

  Hidden Pins Using *FAMILY

  The *FAMILY line can also be used to expose a node inside the subcircuit. This is useful for probing and examining voltage values inside the subcircuit from the top level displayed in SpiceNet. To expose a node nested in a subcircuit, add an additional family name at the end of the list preceded by a pound symbol (#).

For example:
.SUBCKT LM714 1 2 3 4 5 10
**FAMILY ANALOG ANALOG ANALOG ANALOG ANALOG #ANALOG*

This example shows the five subcircuit connections. The last #ANALOG will cause a sixth editable node to be exposed inside SpiceNet from the properties dialog of the LM741. In the part's properties dialog you will be able to assign a node name to the exposed node, and thus connect it to any other place in the circuit that has the same node name.

- Add *PINOUT Line for PCB export.
  The format for a *PINOUT line in a library file is:

  **PINOUT package_name pin_number pin_number ; pin_number pin_number: uncommitted pins*

  The package_name is separated by spaces from the *PINOUT and the pin list. Each pin_number in a pin list is separated by a space. If there is more than one component in the package, the second sequence of numbers follows the first, separated by a semicolon. The pin_numbers in a pin list represent the actual pin numbers used by the manufacturer. The order that the pin numbers appear must match the order of the connection on the .subckt line or, in the case of primitive parts, the order that IsSpice4 expects.

  An Example for a National Instruments AD822:
  **pinout SOIC 3 2 8 4 1;5 6 8 4 7*
  **pinout Cerdip 3 2 8 4 1;5 6 8 4 7*

  If the package has pins that are not represented on the subcircuit, any symbolic name can be given on the *Pinout line, along with the pin number. Place all such pin descriptions at the end of the line following a colon. The name will appear in the Footprint Pins Assignment dialog. These pins can be renamed in the Port column. However, hidden pins can't be added in within this dialog. Users first have to modify the *pinout line in .lib files to get the hidden pins shown for renaming. The following is an example of a LS04 digital inverter that has uncommitted pins, no VCC, and GND connections for simulation:

  .SUBCKT LS04 1 2
  **pinout W 1 2;3 4;5 6;9 8;11 10;13 12:VCC=14 GND=7*

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